

36 V Fully-Differential Programmable-Gain Instrumentation Amplifier with 25 pA Input Bias Current

FEATURES

- ▶ Pin-Programmable Gains:
 - ▶ $G = 0.25, 0.5, 1, 2, 4, 8, 16 \text{ V/V} + \text{Shutdown}$
- ▶ Fully Differential Outputs
- ▶ Gain Error: 0.015% (Max)
- ▶ Gain Error Drift: 1 ppm/°C (Max)
- ▶ CMRR: 103 dB (Min), $G = 16$
- ▶ Input Bias Current: 25 pA (Max)
- ▶ Input Offset Voltage: 92 μV (Max), $G = 16$
- ▶ Input Offset Voltage Drift: 1.7 $\mu\text{V}/^\circ\text{C}$ (Max), $G = 16$
- ▶ -3 dB Bandwidth: 4 MHz, $G = 16$
- ▶ Input Noise Density: 8 nV/ $\sqrt{\text{Hz}}$, $G = 16$
- ▶ Slew Rate: 12 V/ μs , $G = 16$
- ▶ Adjustable Output Common Mode Voltage
- ▶ Quiescent Supply Current: 4.4 mA
- ▶ Supply Voltage Range: $\pm 4.5 \text{ V}$ to $\pm 18 \text{ V}$
- ▶ -40°C to +105°C Specified Temperature Range
- ▶ Small 12-Lead 4 mm $\times$ 4 mm DFN (LFCSP) Package

APPLICATIONS

- ▶ Data Acquisition Systems
- ▶ Biomedical Instrumentation
- ▶ Test and Measurement Equipment
- ▶ Differential ADC Drivers
- ▶ Single-Ended-to-Differential Conversion
- ▶ Multiplexed Applications

TYPICAL APPLICATION

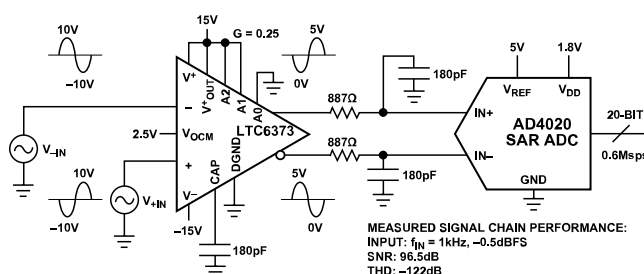


Figure 1. Interfacing a 40 V_{P-P} Ground-Referenced Differential Input Signal to a 5 V ADC

GENERAL DESCRIPTION

The LTC6373 is a precision instrumentation amplifier with fully differential outputs which includes a closely-matched internal resistor network to achieve excellent CMRR, offset voltage, gain error, gain drift, and gain nonlinearity. The user can easily program the gain to one of seven available settings through a 3-bit parallel interface (A2 to A0). The 8th state puts the part in shutdown which reduces the current consumption to 220 μA . Unlike a conventional voltage feedback amplifier, the LTC6373 maintains nearly the same bandwidth across all its gain settings.

The LTC6373 features fully differential outputs to drive high performance, differential-input ADCs. The output common mode voltage is independently adjustable via the V_{OCM} pin. The combination of high impedance inputs, DC precision, low noise, low distortion, and high-speed differential ADC drive makes the LTC6373 an ideal candidate for optimizing data acquisition systems.

The LTC6373 is available in a 12-lead 4 mm $\times$ 4 mm DFN (LFCSP) package and is fully specified over the -40°C to +105°C temperature range.

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REVISION HISTORY

8/2023—Rev. 0 to Rev. A

Updated Format (Universal).....	1
Changes to Features Section.....	1
Change to General Description Section.....	1
Changes to Figure 1.....	1
Deleted Figure 2; Renumbered Sequentially.....	1
Changes to Electrical Characteristics Section and Table 1.....	3
Changes to Absolute Maximum Ratings Section.....	7
Added Thermal Resistance Section and Table 3; Renumbered Sequentially.....	7
Changes to Figure 2.....	8
Changes to Typical Performance Characteristics Section.....	9
Changes to Valid Input and Output Range Section and Figure 78.....	24
Added Figure 79 to Figure 84; Renumbered Sequentially.....	24
Changes to Diamond Plot Interpretation Section.....	26
Changes to Figure 90.....	30
Changes to Figure 102.....	36
Changes to Figure 105.....	37
Changes to Ordering Guide.....	39
Added Evaluation Boards.....	39

8/2020—Revision 0: Initial Version

SPECIFICATIONS

ELECTRICAL CHARACTERISTICS

$V^+ = V_{OUT}^+ = 15\text{ V}$, $V^- = -15\text{ V}$, $V_{ICM} = V_{OCM} = \text{DGND} = 0\text{ V}$, $G = 1$ ($A_2 = 5\text{ V}$, $A_1 = A_0 = 0\text{ V}$). V_S is defined as $(V^+ - V^-)$. V_{ICM} is defined as $(V_{IN} + V_{-IN})/2$. V_{OUTCM} is defined as $(V_{OUT} + V_{-OUT})/2$. $V_{OUTDIFF}$ is defined as $(V_{OUT} - V_{-OUT})$, $T_A = 25^\circ\text{C}$ unless otherwise noted.

Table 1.

Parameter	Symbol	Test Conditions/Comments	Min	Typ	Max	Unit
DIFFERENTIAL GAIN						
Differential Gain Range	G_{DIFF}	$G = 16, 8, 4, 2, 1, 0.5, 0.25$	0.25		16	V/V
Differential Gain Error ¹	ΔG_{DIFF}	$G = 16, 8, 4, 2, 1, 0.5, 0.25$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$		0.003	0.015	%
Differential Gain Drift ^{2, 3}	$\Delta G_{DIFF}/\Delta T$			0.25	1	ppm/ $^\circ\text{C}$
Differential Gain Nonlinearity ¹	GNL	$V_{OUTDIFF} = 40\text{ V}_{P-P}$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$		1	3	ppm
					10	ppm
DIFFERENTIAL OFFSET VOLTAGE (INPUT REFERRED) ⁴						
	V_{OSDIFF}	$G = 16, 8, 4, 2, 1, 0.5, 0.25$ $T_A = -40^\circ\text{C to } +85^\circ\text{C}$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$		10 + 40/G	80 + 192/G 250 + 400/G 1120 + 1120/G	μV μV μV
Differential Offset Voltage Drift (Input Referred) ³	$\Delta V_{OSDIFF}/\Delta T$	$G = 16, 8, 4, 2, 1, 0.5, 0.25$ $T_A = -40^\circ\text{C to } +85^\circ\text{C}$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$		0.3 + 0.5/G	1.5 + 2.5/G	$\mu\text{V}/^\circ\text{C}$
Differential Offset Voltage Hysteresis (Input Referred) ^{2, 5}		$G = 16, 8, 4, 2, 1, 0.5, 0.25$		2 + 1.5/G 10 + 15/G	5 + 5.5/G	$\mu\text{V}/^\circ\text{C}$ μV
INPUT CHARACTERISTICS						
Input Bias Current ^{4, 6}	I_B	Active $T_A = -40^\circ\text{C to } +85^\circ\text{C}$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$ Shutdown ($A_2 = A_1 = A_0 = 5\text{ V}$)		2	25 100 600	pA pA pA
Input Offset Current ^{4, 6}	I_{OS}	Active $T_A = -40^\circ\text{C to } +85^\circ\text{C}$ $T_A = -40^\circ\text{C to } +105^\circ\text{C}$ Shutdown ($A_2 = A_1 = A_0 = 5\text{ V}$)		20 2	25 60 150	pA pA pA
Input Resistance	R_{IN}	Differential mode Common mode		5 5×10^{12} 5×10^{12}		Ω Ω Ω
Input Capacitance	C_{IN}			15		pF
Input Voltage Range	V_{INR}	$T_A = -40^\circ\text{C to } +105^\circ\text{C}$	$V^- + 3$ $V^- + 3.25$		$V^+ - 3$ $V^+ - 3$	V V
NOISE						
Differential Input Voltage Noise Density	e_n	$f = 10\text{ kHz}$ $G = 16$ $G = 8$ $G = 4$ $G = 2$ $G = 1$ $G = 0.5$ $G = 0.25$		8 8.4 9.5 12.2 18.7 26.4 41		$\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$ $\text{nV}/\sqrt{\text{Hz}}$
Differential Input Voltage Noise		0.1 Hz to 10 Hz $G = 16$ $G = 8$ $G = 4$ $G = 2$ $G = 1$		1.1 1.2 1.3 1.5 1.8		μV_{P-P} μV_{P-P} μV_{P-P} μV_{P-P} μV_{P-P}

SPECIFICATIONS

Table 1. (Continued)

Parameter	Symbol	Test Conditions/Comments	Min	Typ	Max	Unit
Input Current Noise Density	i_n	$G = 0.5$		2.4		$\mu V_{P-P}/\sqrt{Hz}$
Input Current Noise		$G = 0.25$		4.2		$\mu V_{P-P}/\sqrt{Hz}$
Common Mode Voltage Noise Density		$f = 10 \text{ kHz}$		1		$fA/\sqrt{Hz}$
	e_{nVOCM}	0.1 Hz to 10 Hz		100		$fA_{P-P}/\sqrt{Hz}$
		$f = 10 \text{ kHz}$		24		$nV/\sqrt{Hz}$
COMMON MODE REJECTION RATIO (INPUT REFERRED)						
Input Common Mode Rejection Ratio (Input Referred) $\Delta V_{ICM}/\Delta V_{OSDIFF}$ ⁷	CMRR	DC to 60 Hz, 1 k Ω source Imbalance, $V_{ICM} = \pm 10 \text{ V}$				
		$G = 16$	103	119		dB
		$G = 16, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	98			dB
		$G = 8$	100	113		dB
		$G = 8, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	98			dB
		$G = 4$	94	107		dB
		$G = 4, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	92			dB
		$G = 2$	88	101		dB
		$G = 2, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	86			dB
		$G = 1$	82	95		dB
		$G = 1, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	80			dB
		$G = 0.5$	83	95		dB
		$G = 0.5, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	80			dB
		$G = 0.25$	80	95		dB
		$G = 0.25, T_A = -40^\circ\text{C to } +105^\circ\text{C}$	75			dB
Output Common Mode Rejection Ratio (Input Referred) $\Delta V_{OCM}/\Delta V_{OSDIFF}$ ^{2, 7}	CMRRIO	$V_{OCM} = \pm 13 \text{ V}$	75	95		dB
POWER SUPPLY REJECTION RATIO						
Differential Power Supply Rejection Ratio ($\Delta V_S/\Delta V_{OSDIFF}$) ^{2, 8}	PSRR	$V_S = \pm 4.5 \text{ V to } \pm 18 \text{ V}$				
		$G = 16$	105	142		dB
		$G = 8$	102	139		dB
		$G = 4$	102	136		dB
		$G = 2$	100	133		dB
		$G = 1$	98	130		dB
		$G = 0.5$	95	125		dB
		$G = 0.25$	92	120		dB
Output Common Mode Power Supply Rejection Ratio ($\Delta V_S/\Delta V_{OSCM}$) ^{2, 8}	PSRRCM	$V_S = \pm 4.5 \text{ V to } \pm 18 \text{ V}$	110	135		dB
OUTPUT ²						
Output Voltage, High, Either Output Pin	V_{OUT}	$I_L = 0 \text{ mA}, V_S = \pm 4.5 \text{ V}$	$V_{OUT}^+ - 0.6$	$V_{OUT}^+ - 0.3$		V
		$I_L = -5 \text{ mA}, V_S = \pm 4.5 \text{ V}$	$V_{OUT}^+ - 1.1$	$V_{OUT}^+ - 0.7$		V
		$I_L = 0 \text{ mA}, V_S = \pm 15 \text{ V}$	$V_{OUT}^+ - 1.8$	$V_{OUT}^+ - 1.1$		V
		$I_L = -5 \text{ mA}, V_S = \pm 15 \text{ V}$	$V_{OUT}^+ - 1.9$	$V_{OUT}^+ - 1.3$		V
Output Voltage, Low, Either Output Pin	V_{OUT}	$I_L = 0 \text{ mA}, V_S = \pm 4.5 \text{ V}$		$V^- + 0.3$	$V^- + 0.6$	V
		$I_L = 5 \text{ mA}, V_S = \pm 4.5 \text{ V}$		$V^- + 0.6$	$V^- + 1$	V
		$I_L = 0 \text{ mA}, V_S = \pm 15 \text{ V}$		$V^- + 1.1$	$V^- + 1.8$	V
		$I_L = 5 \text{ mA}, V_S = \pm 15 \text{ V}$		$V^- + 1.2$	$V^- + 1.9$	V
Output Short-Circuit Current, Either Output Pin, Sinking	I_{SC}	$V_S = \pm 4.5 \text{ V}$	27	39		mA
		$V_S = \pm 15 \text{ V}$	35	47		mA
Output Short-Circuit Current, Either Output Pin, Sourcing	I_{SC}	$V_S = \pm 4.5 \text{ V}$	23	33		mA
		$V_S = \pm 15 \text{ V}$	29	38		mA

SPECIFICATIONS

Table 1. (Continued)

Parameter	Symbol	Test Conditions/Comments	Min	Typ	Max	Unit
Output Balance ($\Delta V_{OUTCM}/\Delta V_{OUTDIFF}$)	BAL	$V_{OUTDIFF} = \pm 10$ V Single-ended input Differential input		–80 –90	–70 –75	dB dB
COMMON MODE GAIN ($\Delta V_{OUTCM}/\Delta V_{OCM}$) ²	G_{CM}	$V_S = \pm 4.5$ V, $V_{OCM} = \pm 3$ V $V_S = \pm 15$ V, $V_{OCM} = \pm 13$ V		1 1		V/V V/V
Common Mode Gain Error $100 \times (G_{CM} - 1)$	ΔG_{CM}	$V_S = \pm 4.5$ V, $V_{OCM} = \pm 3$ V $V_S = \pm 15$ V, $V_{OCM} = \pm 13$ V		0.05 0.05	0.1 0.1	% %
COMMON MODE OFFSET VOLTAGE ($V_{OUTCM} - V_{OCM}$)	V_{OSCM}	$T_A = -40^\circ\text{C}$ to $+105^\circ\text{C}$		1	40 50	mV mV
V_{OCM} PIN ²						
Voltage Range for the V_{OCM} Pin (Guaranteed by ΔG_{CM})	V_{OUTCMR}	$V_S = \pm 4.5$ V $V_S = \pm 15$ V	$V^- + 1.5$ $V^- + 2$		$V_{OUT}^+ - 1.5$ $V_{OUT}^+ - 2$	V V
Self-Biased Voltage at the V_{OCM} Pin	V_{OCM}	V_{OCM} not connected	$(V_{OUT}^+ + V^-)/2 - 0.1$	$(V_{OUT}^+ + V^-)/2$	$(V_{OUT}^+ + V^-)/2 + 0.1$	V
Input Resistance, V_{OCM} Pin	R_{INVOCM}		1.9	2.3	2.7	M Ω
DGND PIN ²						
Voltage Range for the DGND Pin	V_{DGND}		V^-	0	$V^+ - 2.5$	V
DGND Pin Current	I_{DGND}	DGND = 5 V, A2 = A1 = A0 = 15 V	–7	–4	–1	μA
DIGITAL INPUT ²						
Digital Input (A2/A1/A0) Logic Low	V_{IL}	Referred to DGND	DGND		DGND + 0.6	V
Digital Input (A2/A1/A0) Logic High	V_{IH}	Referred to DGND	DGND + 1.5		V^+	V
Digital Input (A2/A1/A0) Pin Current	$I_{A2/A1/A0}$	A2/A1/A0 = 5 V		8	12	μA
DYNAMIC RESPONSE						
–3 dB Bandwidth	f_{-3dB}	$G = 16$ $G = 8$ $G = 4$ $G = 2$ $G = 1$ $G = 0.5$ $G = 0.25$		4 5.5 6 6.5 6.5 7 7.5		MHz MHz MHz MHz MHz MHz MHz
Slew Rate ²	SR	$G = 16$, $V_{OUTDIFF} = 40$ V _{P-P} Step, $R_L = 2$ k Ω	7.5	12		V/ μs
Settling Time	t_s	$G = 16$, $V_{OUTDIFF} = 8$ V _{P-P} Step, $R_L = 1$ k Ω 0.1% 0.01% 0.0015% (16-bit) 4 ppm (18-bit)		2.1 2.25 2.4 2.7		μs μs μs μs
Total Harmonic Distortion	THD	$G = 1$, $V_{OUTDIFF} = 10$ V _{P-P} , $R_L = 2$ k Ω $f = 1$ kHz $f = 10$ kHz		–115 –110		dB dB
TIMING CHARACTERISTICS						
Turn-On Time	t_{ON}			10		μs
Turn-Off Time	t_{OFF}			5		μs
Gain Switching Time				5		μs
SUPPLY						
Supply Voltage Range ²	V_S	Guaranteed by PSRR	9		36	V
Supply Current	I_S	Active $T_A = -40^\circ\text{C}$ to $+105^\circ\text{C}$ Shutdown (A2 = A1 = A0 = 5 V) ²		4.4 220	4.75 600	mA mA μA

SPECIFICATIONS

- ¹ This parameter is measured in a high speed automatic tester that does not measure the thermal effects with longer time constants. The magnitude of these thermal effects is dependent on the package used, PCB layout, heat sinking, and air flow conditions.
- ² This specification is applied over the full operating temperature range.
- ³ Guaranteed by design.
- ⁴ ESD (Electrostatic Discharge) sensitive device. ESD protection devices are used extensively internal to the LTC6373; however, high electrostatic discharge can damage or degrade the device. Use proper ESD handling precautions.
- ⁵ Hysteresis in output voltage is created by mechanical stress that differs depending on whether the IC was previously at a higher or lower temperature. Output voltage is always measured at 25°C, but the IC is cycled to the hot or cold temperature limit before successive measurements. For instruments that are stored in well controlled temperatures (within 20 or 30 degrees of operational temperature), hysteresis is usually not a significant error source. Typical Hysteresis is the worst case of differential offset measured between 25°C to -40°C to 25°C thermal cycle and 25°C to 105°C to 25°C thermal cycle.
- ⁶ Input bias current is defined as the maximum of the input currents flowing into either of the input pins (-IN and +IN). Input Offset current is defined as the difference between the input currents ($I_{OS} = I_{B^+} - I_{B^-}$).
- ⁷ Input CMRR (CMRR) is defined as the ratio of the change in the input common mode voltage at the pins +IN or -IN to the change in differential input referred offset voltage. Output CMRR (CMRRIO) is defined as the ratio of the change in the voltage at the VOCM pin to the change in differential input referred offset voltage.
- ⁸ Differential power supply rejection ratio (PSRR) is defined as the ratio of the change in supply voltage to the change in differential input referred offset voltage. Common mode power supply rejection ratio (PSRR_{CM}) is defined as the ratio of the change in supply voltage to the change in the common mode offset voltage.

ABSOLUTE MAXIMUM RATINGS

Table 2.

Parameter	Rating
Supply Voltages	
V^+	V^- to $(V^- + 40\text{ V})$
V^+_{OUT}	V^- to $(V^+ + 0.3\text{ V})$
V_{OCM}	$(V^- - 0.3\text{ V})$ to $(V^+_{OUT} + 0.3\text{ V})$
A0, A1, A2, DGND	$(V^- - 0.3\text{ V})$ to $(V^+ + 0.3\text{ V})$
+IN, -IN	
Common Mode	$(V^- - 0.3\text{ V})$ to $(V^+ + 0.3\text{ V})$
Differential	$\pm 20\text{ V}$
Output Current (+OUT, -OUT) ¹	40 mA _{RMS}
Output Short-Circuit Duration (+OUT, -OUT) ²	Thermally Limited
Operating and Specified Temperature Range ^{3, 4}	
LTC6373I	-40°C to $+85^\circ\text{C}$
LTC6373S	-40°C to $+105^\circ\text{C}$
Maximum Junction Temperature (T_{JMAX})	150°C
Storage Temperature Range	-65°C to $+150^\circ\text{C}$

¹ The LTC6373 is capable of producing peak output currents in excess of 40 mA. Current density limitations within the IC require the continuous RMS current supplied by the output (sourcing or sinking) over the operating lifetime of the part be limited to under 40 mA (Absolute Maximum).

² A heat sink may be required to keep the junction temperature below absolute maximum when the output is shorted indefinitely.

³ The LTC6373I is guaranteed functional over the operating temperature range of -40°C to $+85^\circ\text{C}$. The LTC6373S is guaranteed functional over the operating temperature range of -40°C to $+105^\circ\text{C}$.

⁴ The LTC6373I is guaranteed to meet specified performance from -40°C to $+85^\circ\text{C}$. The LTC6373S is guaranteed to meet specified performance from -40°C to $+105^\circ\text{C}$.

Stresses at or above those listed under Absolute Maximum Ratings may cause permanent damage to the product. This is a stress rating only; functional operation of the product at these or any other conditions above those indicated in the operational section of this specification is not implied. Operation beyond the maximum operating conditions for extended periods may affect product reliability.

THERMAL RESISTANCE

Thermal performance is directly linked to system design and operating environment. Careful attention to the printed circuit board (PCB) thermal design is required. θ_{JC} is the channel to case thermal resistance, channel to bottom of die using die attach epoxy.

Table 3. Thermal Resistance

Package Type	θ_{JA}	θ_{JC}	Unit
05-08-1791	43	3.4	$^\circ\text{C/W}$

ESD CAUTION



ESD (electrostatic discharge) sensitive device. Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.

PIN CONFIGURATION AND FUNCTION DESCRIPTIONS

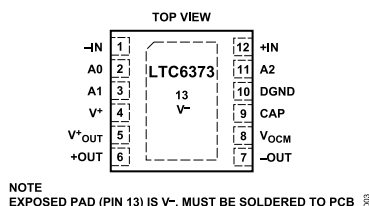


Figure 2. Pin Configuration

Table 4. Pin Function Descriptions

Pin No.	Mnemonic	Description
1	-IN	Inverting Input of Instrumentation Amplifier. Input voltage range is between $V^- + 3\text{ V}$ and $V^+ - 3\text{ V}$.
2	A0	Digital Gain Programming Pin 0. In combination with A2 and A1, the user can choose the desired gain setting for the LTC6373 (refer to Gain Selection section of this data sheet). The logic threshold for the A0 pin is specified with respect to the voltage on the DGND pin (logic low = any voltage between DGND and $\text{DGND} + 0.6\text{ V}$; logic high = any voltage between $\text{DGND} + 1.5\text{ V}$ and V^+). If the A0 pin is left floating, an internal resistor pulls its voltage close to the DGND pin, resulting in a default logic low state for this programming pin.
3	A1	Digital Gain Programming Pin 1. In combination with A2 and A0, the user can choose the desired gain setting for the LTC6373 (refer to Gain Selection section of this data sheet). The logic threshold for the A1 pin is specified with respect to the voltage on the DGND pin (logic low = any voltage between DGND and $\text{DGND} + 0.6\text{ V}$; logic high = any voltage between $\text{DGND} + 1.5\text{ V}$ and V^+). If the A1 pin is left floating, an internal resistor pulls its voltage close to the DGND pin, resulting in a default logic low state for this programming pin.
4	V^+	Positive Power Supply. The operating voltage range for V^+ is $(V^- + 9\text{ V}) \leq V^+ \leq (V^- + 36\text{ V})$.
5	V^+_{OUT}	Positive Power Supply for the Output Differential Amplifier inside the LTC6373 (the amplifier marked as A3 in Figure 76 of this data sheet). V^+_{OUT} pin is normally tied to V^+ pin, however the user may also choose a lower voltage for V^+_{OUT} to save power dissipation or to help protect ADC inputs. The voltage on V^+_{OUT} pin should never be higher than V^+ pin. The operating voltage range for V^+_{OUT} is $(V^- + 9\text{ V}) \leq V^+_{\text{OUT}} \leq V^+$.
6	+OUT	Positive Output Pin of Instrumentation Amplifier.
7	-OUT	Negative Output Pin of Instrumentation Amplifier.
8	V_{OCM}	Output Common Mode Reference Voltage. Voltage applied to this pin sets the output common mode voltage level. If the V_{OCM} pin is left floating, an internal resistor divider creates a default voltage approximately halfway between V^+_{OUT} and V^- . The V_{OCM} pin should be decoupled to ground with a minimum of $0.1\text{ }\mu\text{F}$ bypass capacitor.
9	CAP	Bypass Capacitor Pin. The CAP pin should be decoupled to ground with a 180 pF bypass capacitor.
10	DGND	Reference for Digital Gain Programming Pins (A2/A1/A0). DGND is normally tied to ground, however any voltage between V^- and $V^+ - 2.5\text{ V}$ may also be chosen. If the DGND pin is left floating, an internal resistor divider creates a default voltage approximately halfway between V^+ and V^- . The logic threshold for A2/A1/A0 pins is specified with respect to the DGND pin.
11	A2	Digital Gain Programming Pin 2. In combination with A1 and A0, the user can choose the desired gain setting for the LTC6373 (refer to Gain Selection section of this data sheet). The logic threshold for the A2 pin is specified with respect to the voltage on the DGND pin (logic low = any voltage between DGND and $\text{DGND} + 0.6\text{ V}$; logic high = any voltage between $\text{DGND} + 1.5\text{ V}$ and V^+). If the A2 pin is left floating, an internal resistor pulls its voltage close to the DGND pin, resulting in a default logic low state for this programming pin.
12	+IN	Noninverting Input of Instrumentation Amplifier. Input voltage range is between $V^- + 3\text{ V}$ and $V^+ - 3\text{ V}$.
13	EPAD (V^-)	Exposed Pad (Negative Power Supply). The exposed pad must be soldered to PCB and connected to V^- .

TYPICAL PERFORMANCE CHARACTERISTICS

$V^+ = V_{OUT}^+ = 15\text{ V}$, $V^- = -15\text{ V}$, $V_{ICM} = V_{OCM} = 0\text{ V}$, $T_A = 25^\circ\text{C}$, $G = 1$, unless otherwise noted.

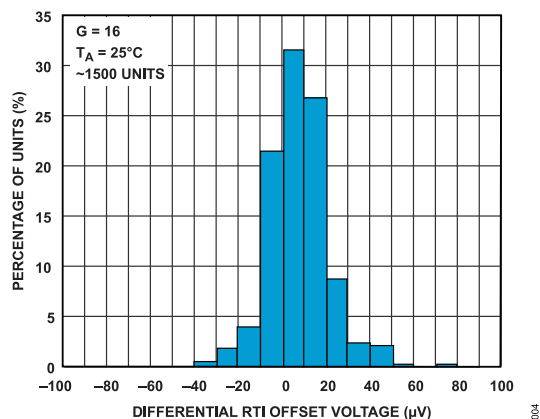


Figure 3. Typical Distribution of Differential RTI Offset Voltage

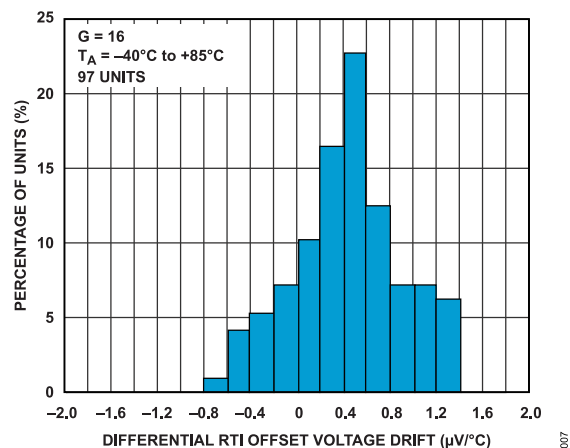


Figure 6. Typical Distribution of Differential RTI Offset Voltage Drift

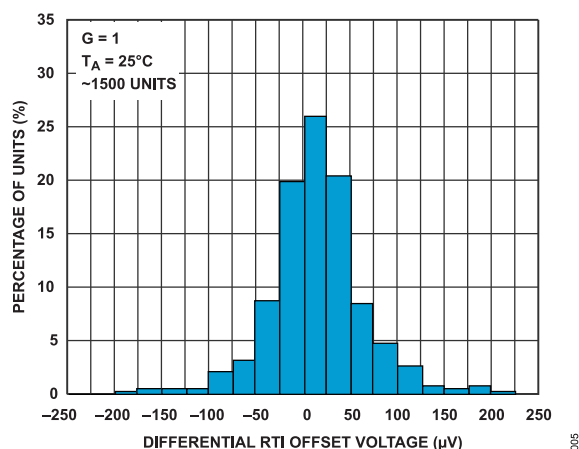


Figure 4. Typical Distribution of Differential RTI Offset Voltage

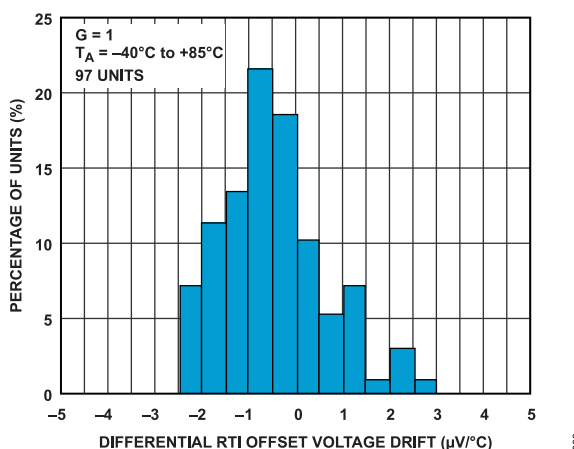


Figure 7. Typical Distribution of Differential RTI Offset Voltage Drift

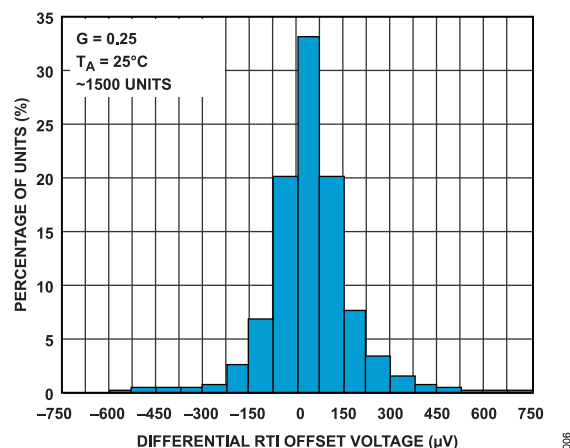


Figure 5. Typical Distribution of Differential RTI Offset Voltage

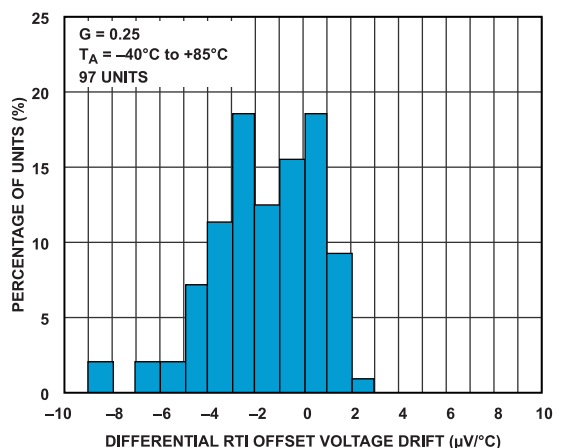


Figure 8. Typical Distribution of Differential RTI Offset Voltage Drift

TYPICAL PERFORMANCE CHARACTERISTICS

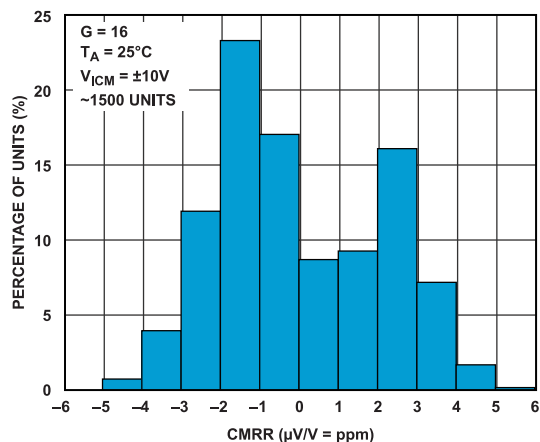


Figure 9. Typical Distribution of CMRR

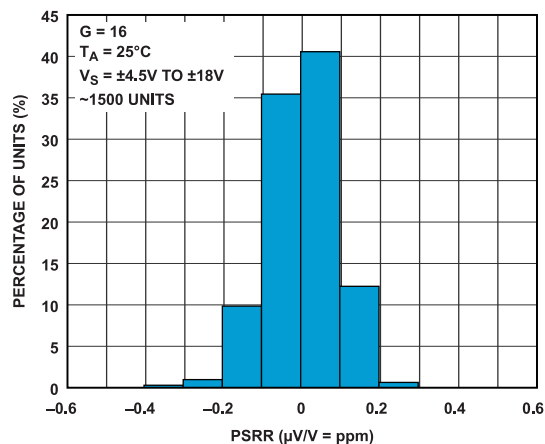


Figure 12. Typical Distribution of Differential PSRR

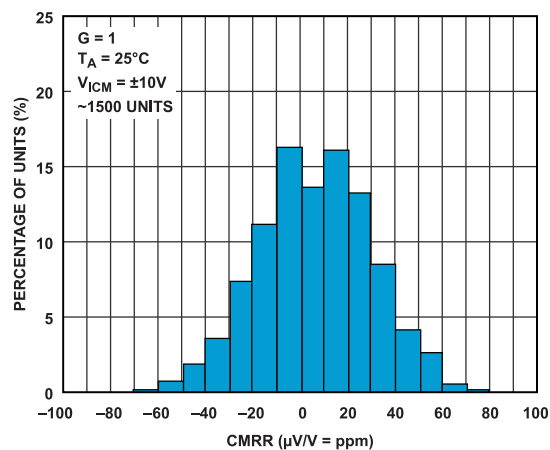


Figure 10. Typical Distribution of CMRR

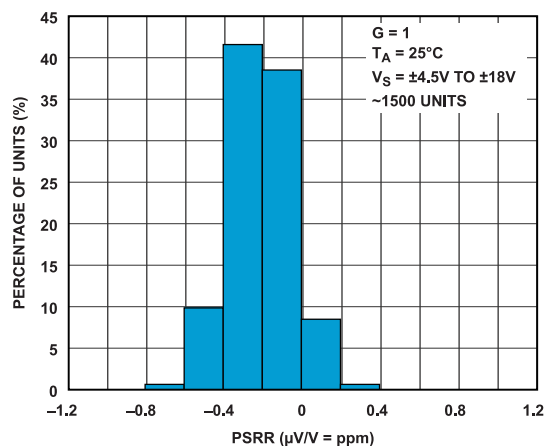


Figure 13. Typical Distribution of Differential PSRR

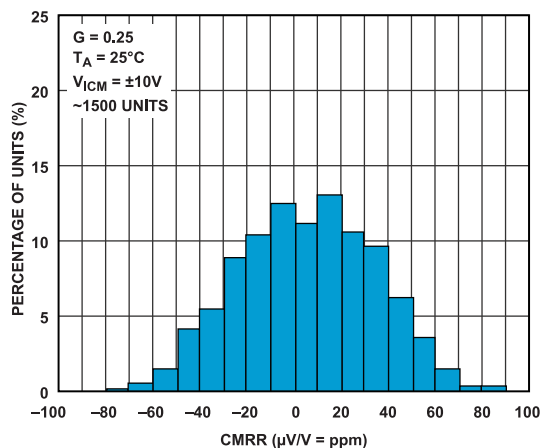


Figure 11. Typical Distribution of CMRR

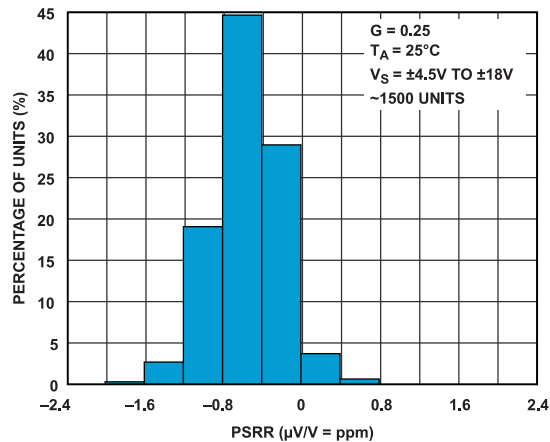


Figure 14. Typical Distribution of Differential PSRR

TYPICAL PERFORMANCE CHARACTERISTICS

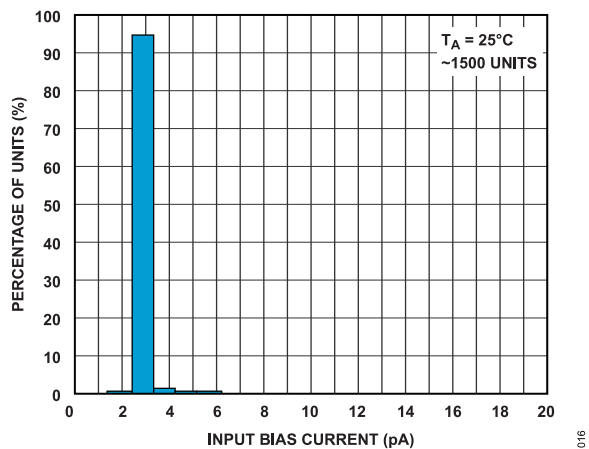


Figure 15. Typical Distribution of Input Bias Current

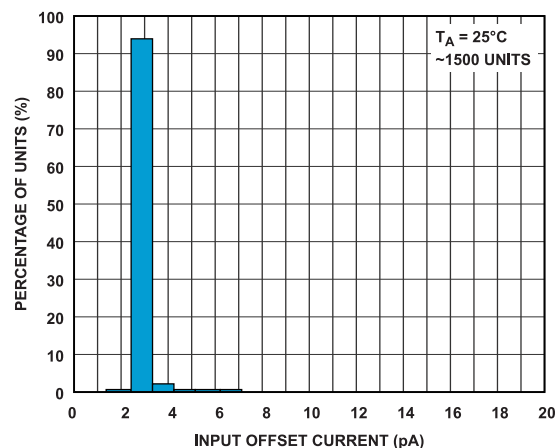


Figure 16. Typical Distribution of Input Offset Current

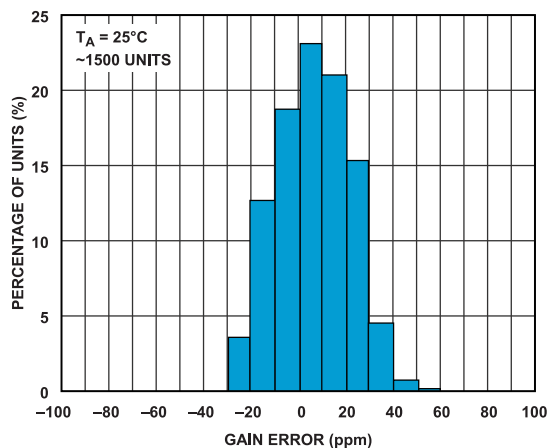


Figure 17. Typical Distribution of Differential Gain Error

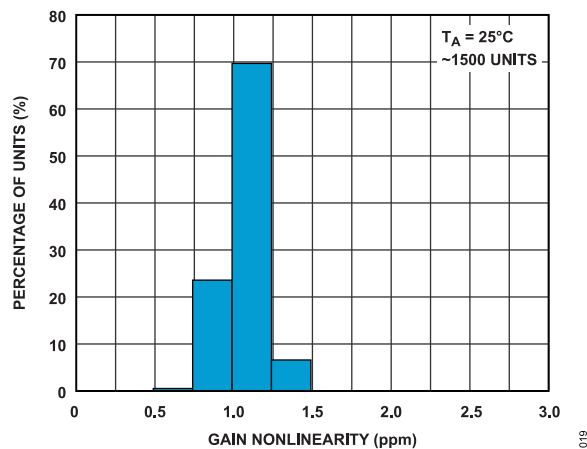


Figure 18. Typical Distribution of Differential Gain Nonlinearity

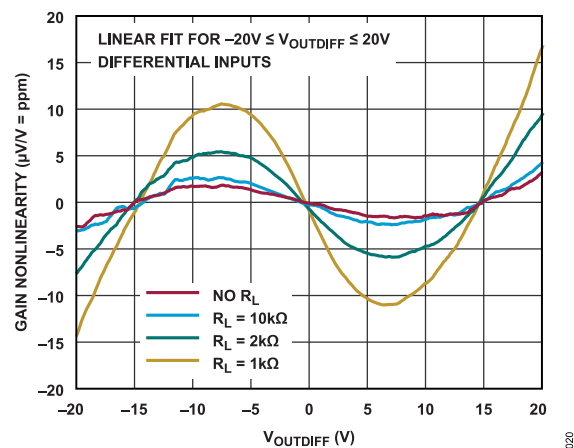


Figure 19. Differential Gain Nonlinearity vs. Output Voltage

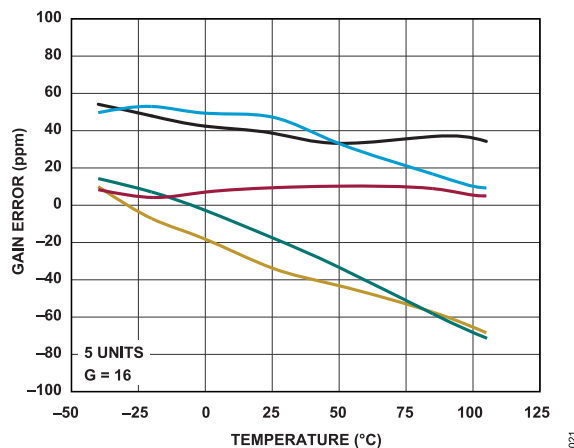


Figure 20. Differential Gain Error vs. Temperature

TYPICAL PERFORMANCE CHARACTERISTICS

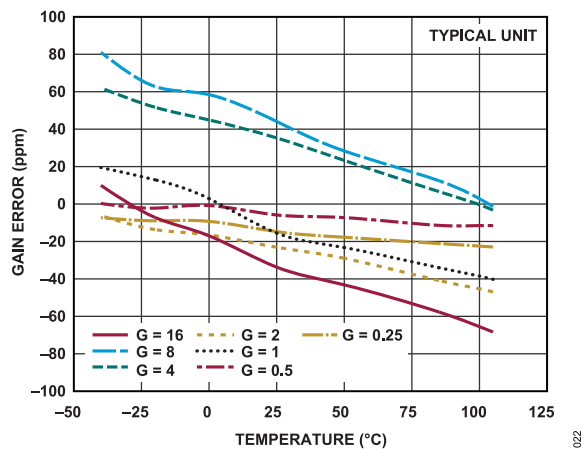


Figure 21. Differential Gain Error vs. Temperature

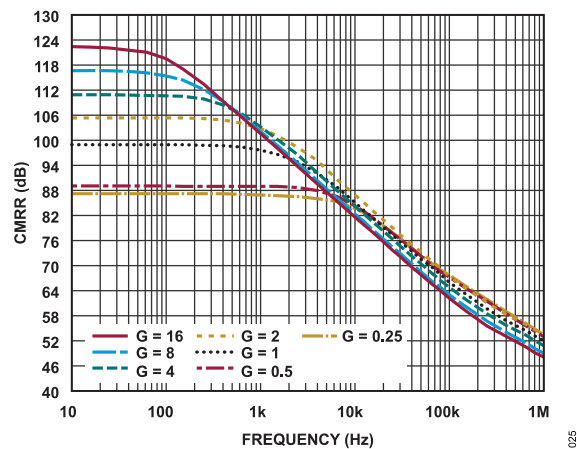


Figure 24. CMRR vs. Frequency

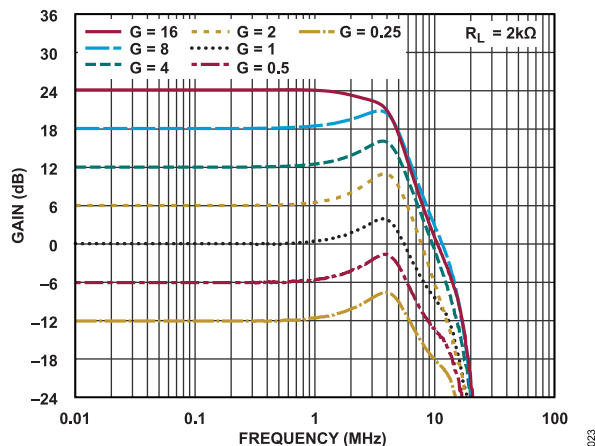


Figure 22. Gain vs. Frequency

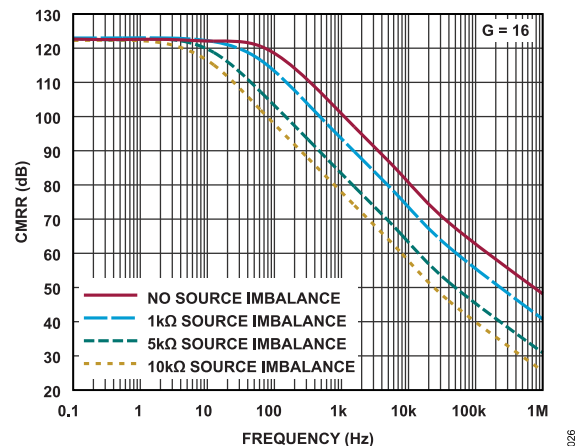


Figure 25. CMRR vs. Frequency With Source Imbalance

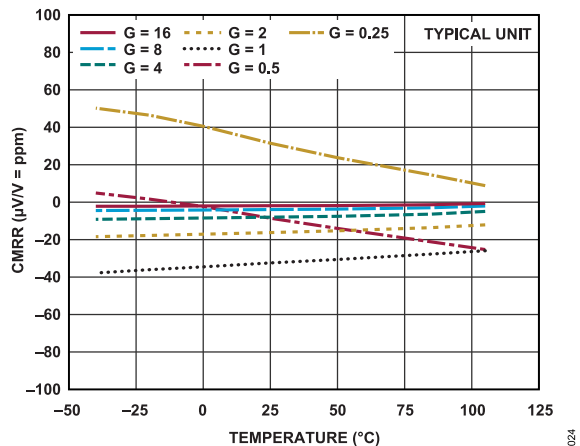


Figure 23. CMRR vs. Temperature

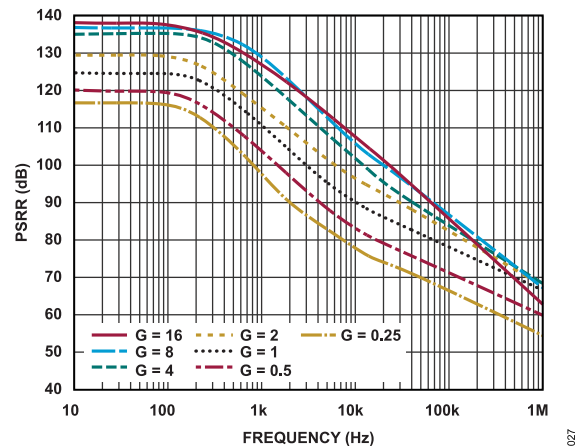


Figure 26. Positive PSRR vs. Frequency, RTI

TYPICAL PERFORMANCE CHARACTERISTICS

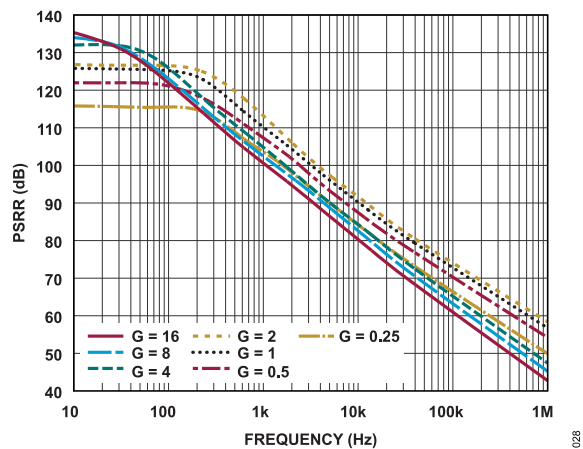


Figure 27. Negative PSRR vs. Frequency, RTI

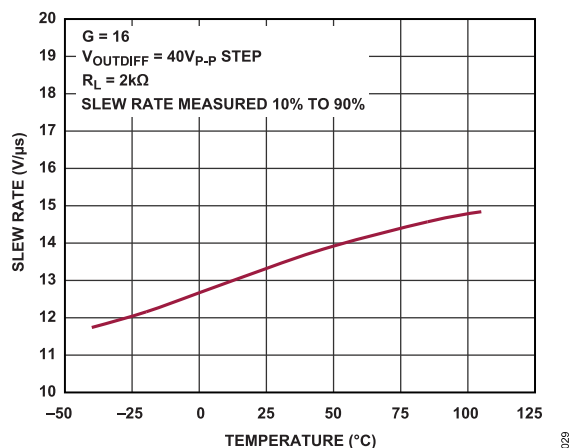


Figure 28. Slew Rate vs. Temperature

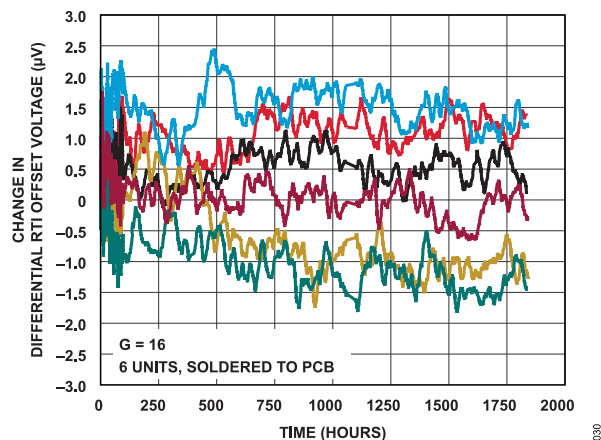


Figure 29. Long Term Differential RTI Offset Voltage Drift

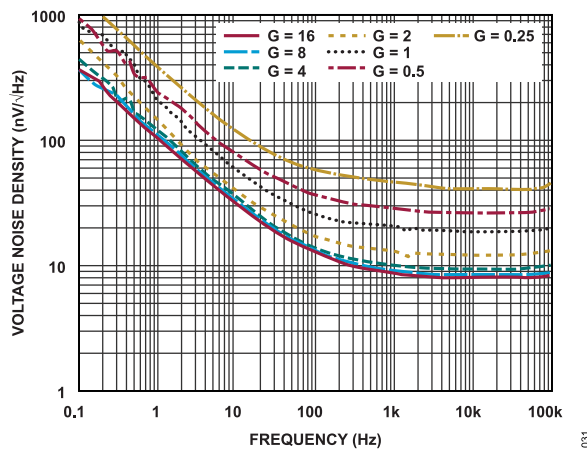


Figure 30. Input Referred Voltage Noise Density vs. Frequency

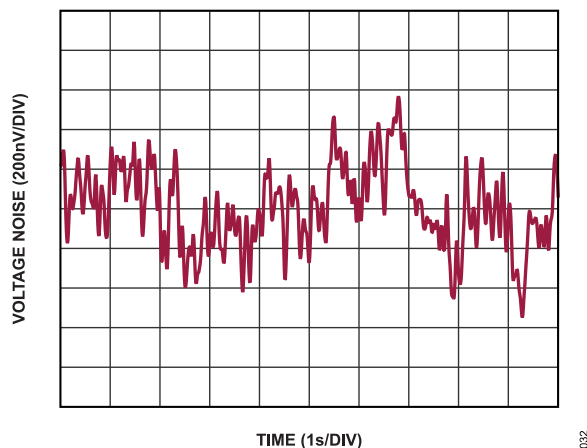


Figure 31. Input Referred 0.1 Hz to 10 Hz Voltage Noise (G = 16)

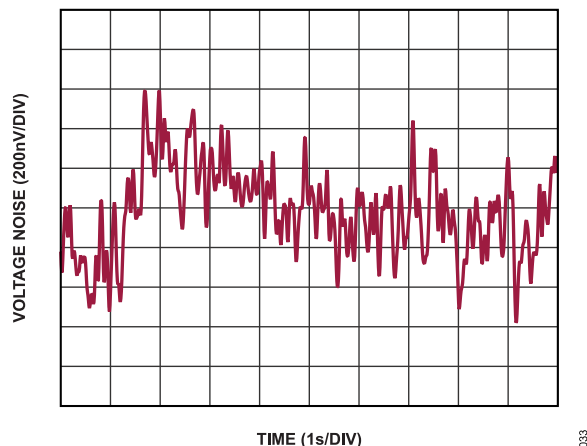


Figure 32. Input Referred 0.1 Hz to 10 Hz Voltage Noise (G = 8)

TYPICAL PERFORMANCE CHARACTERISTICS

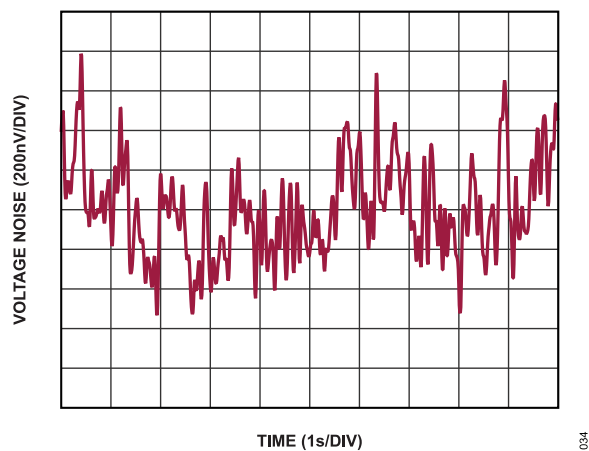
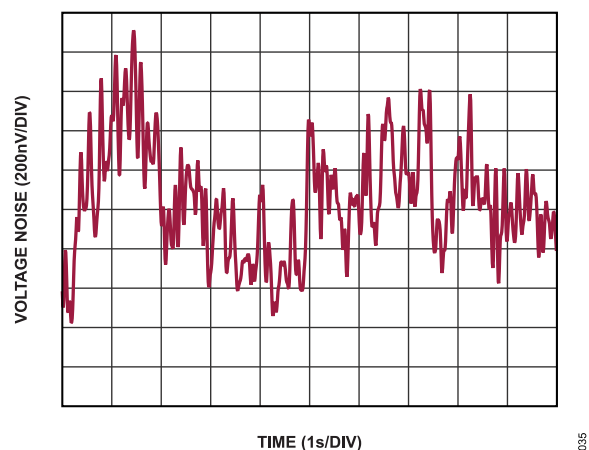
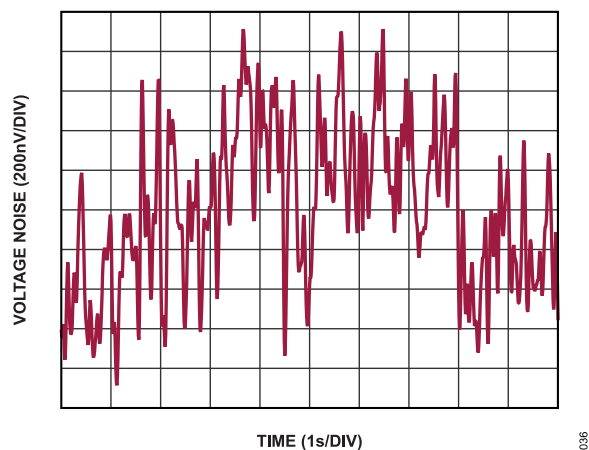
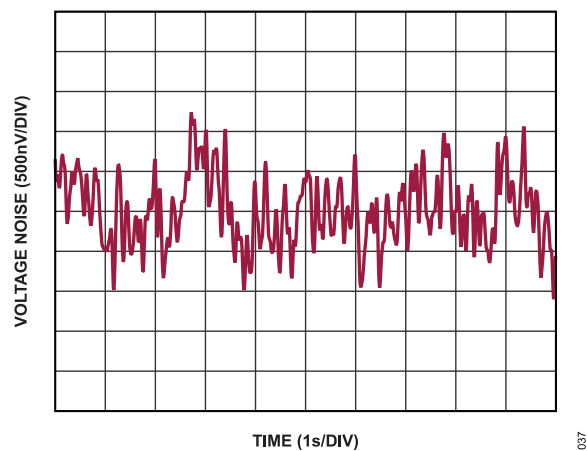
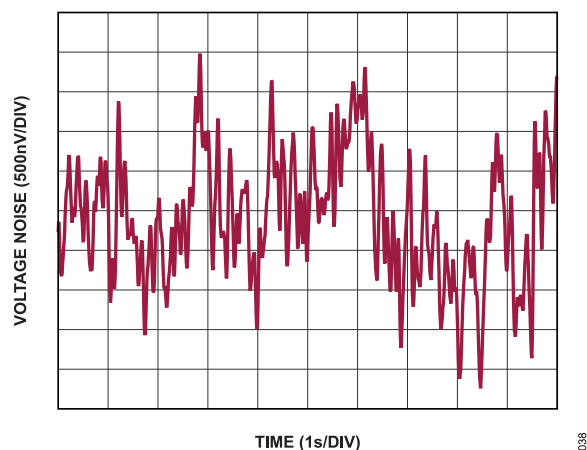
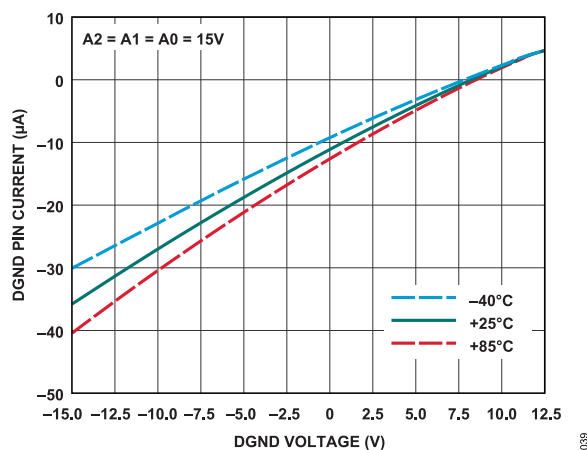
Figure 33. Input Referred 0.1 Hz to 10 Hz Voltage Noise ($G = 4$)Figure 34. Input Referred 0.1 Hz to 10 Hz Voltage Noise ($G = 2$)Figure 35. Input Referred 0.1 Hz to 10 Hz Voltage Noise ($G = 1$)Figure 36. Input Referred 0.1 Hz to 10 Hz Voltage Noise ($G = 0.5$)Figure 37. Input Referred 0.1 Hz to 10 Hz Voltage Noise ($G = 0.25$)

Figure 38. DGND Pin Current vs. DGND Pin Voltage

TYPICAL PERFORMANCE CHARACTERISTICS

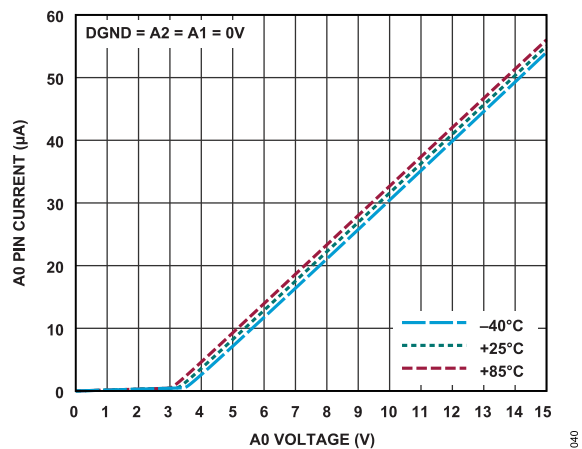


Figure 39. A0 Digital Input Pin Current vs. A0 Digital Input Pin Voltage

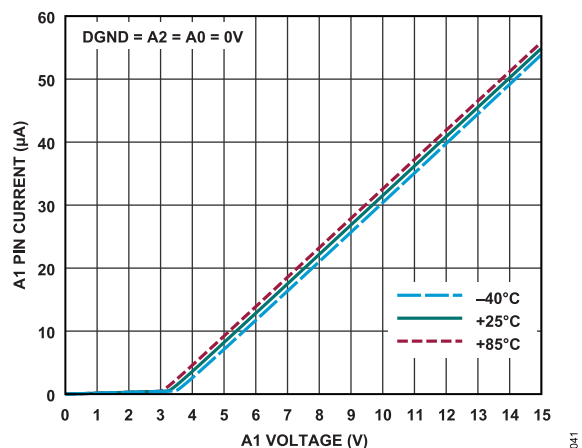


Figure 40. A1 Digital Input Pin Current vs. A1 Digital Input Pin Voltage

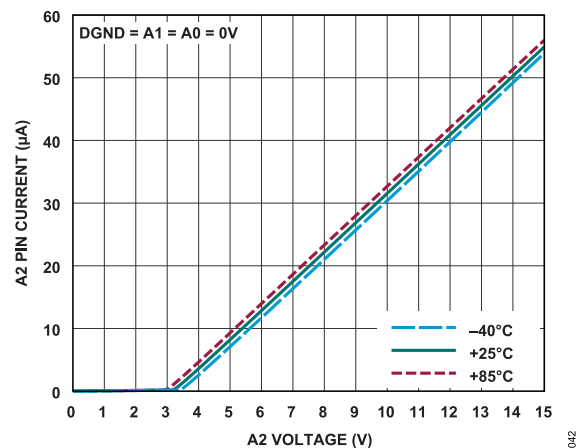


Figure 41. A2 Digital Input Pin Current vs. A2 Digital Input Pin Voltage

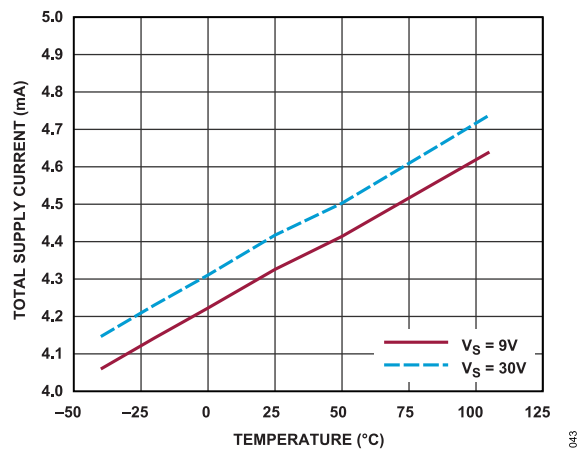


Figure 42. Supply Current vs. Temperature

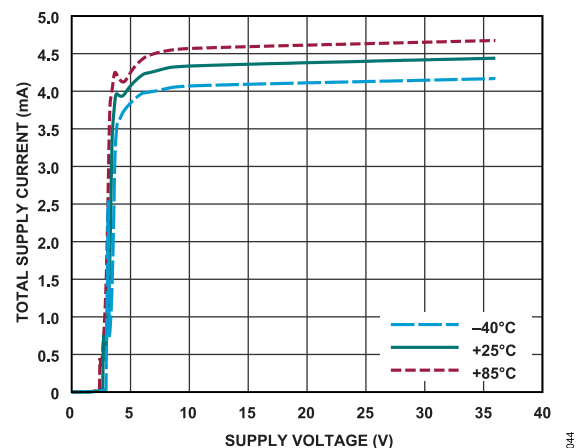


Figure 43. Supply Current vs. Supply Voltage

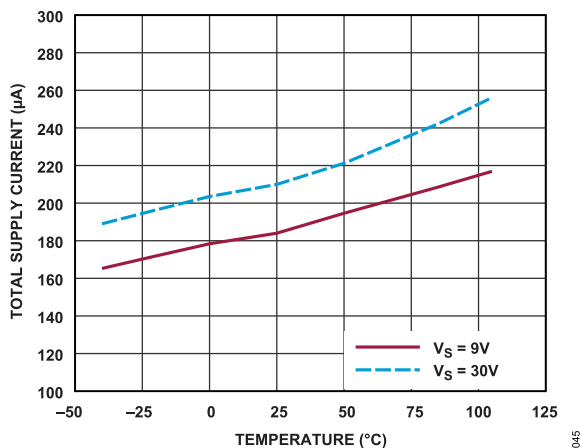


Figure 44. Shutdown Supply Current vs. Temperature

TYPICAL PERFORMANCE CHARACTERISTICS

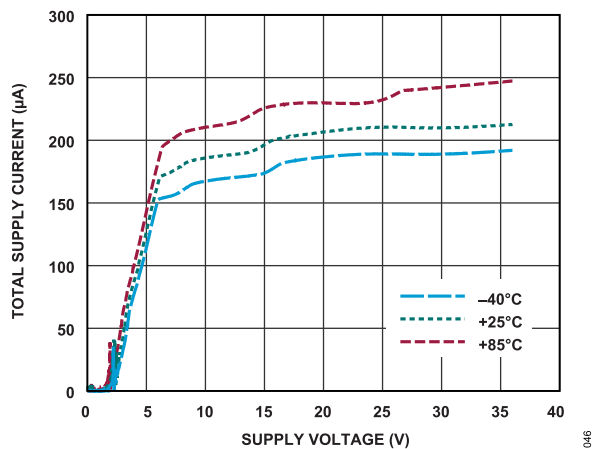


Figure 45. Shutdown Supply Current vs. Supply Voltage

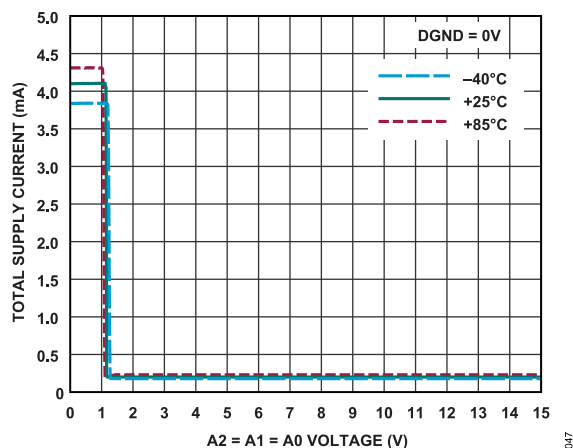


Figure 46. Supply Current vs. Digital Input (A2/A1/A0) Pin Voltage

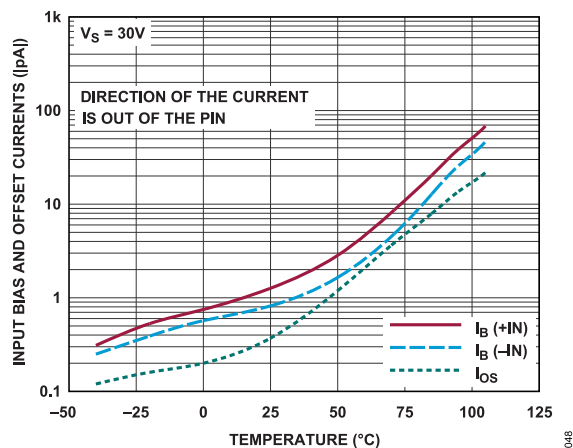


Figure 47. Input Bias Current and Offset Current vs. Temperature

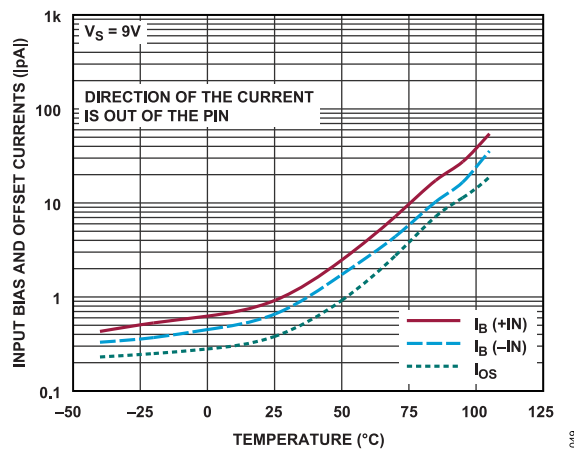


Figure 48. Input Bias Current and Offset Current vs. Temperature

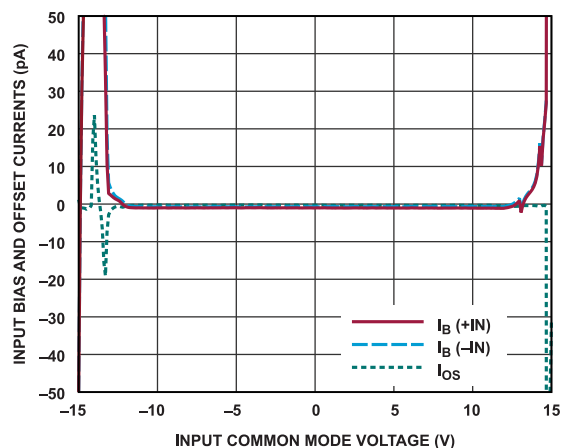


Figure 49. Input Bias Current and Offset Current vs. Input Common Mode Voltage

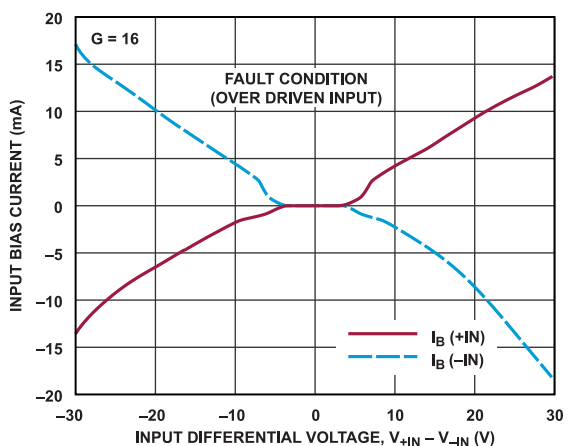


Figure 50. Input Bias Current vs. Input Differential Voltage

TYPICAL PERFORMANCE CHARACTERISTICS

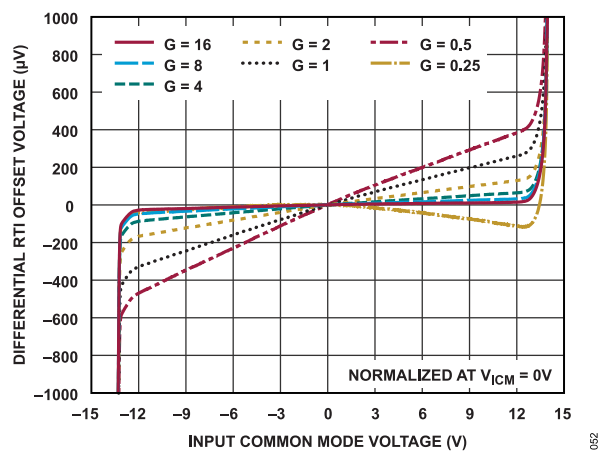


Figure 51. Differential RTI Offset Voltage vs. Input Common Mode Voltage

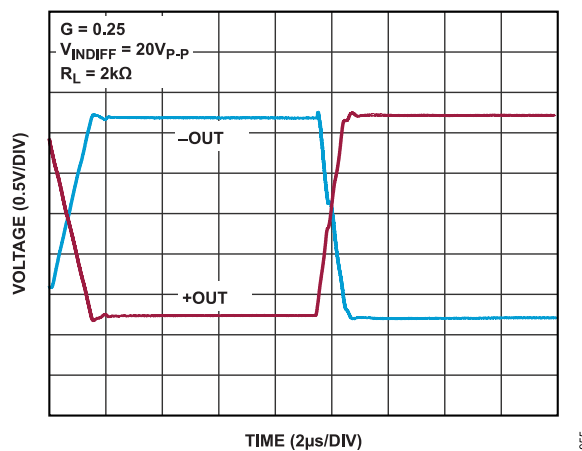


Figure 54. Large Signal Step Response

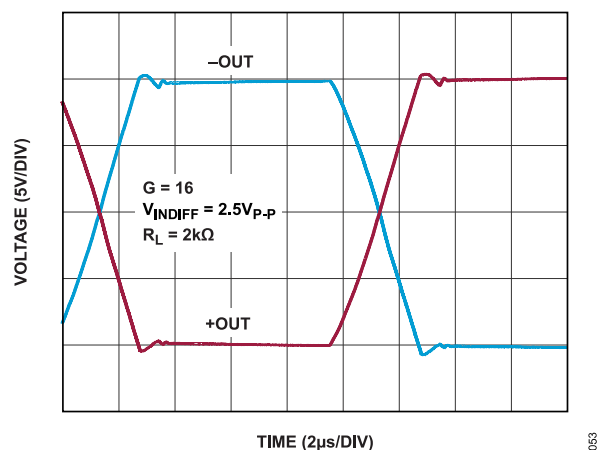


Figure 52. Large Signal Step Response

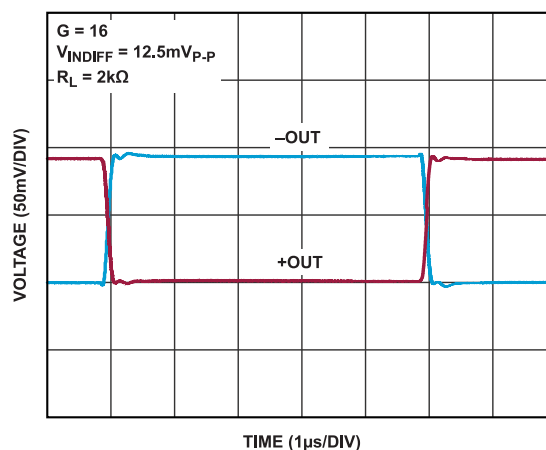


Figure 55. Small Signal Step Response

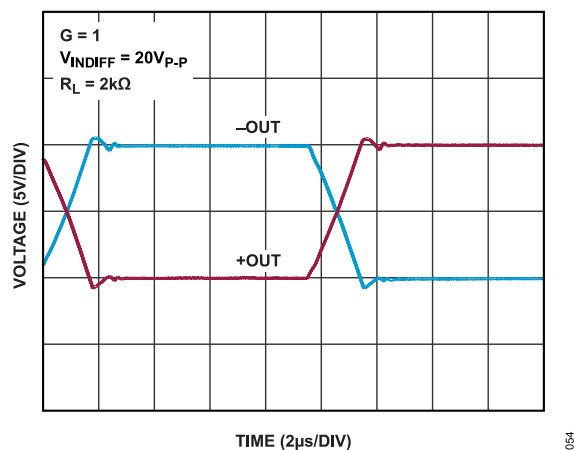


Figure 53. Large Signal Step Response

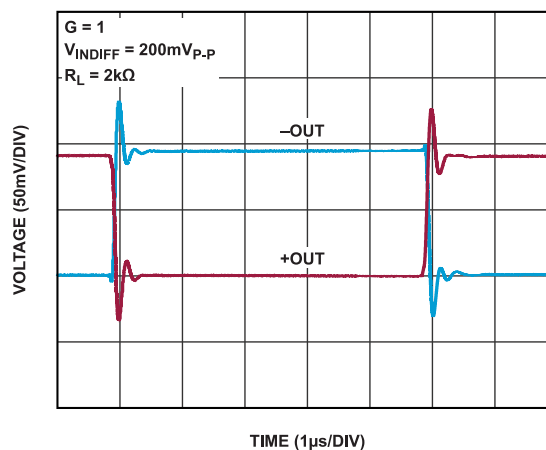


Figure 56. Small Signal Step Response

TYPICAL PERFORMANCE CHARACTERISTICS

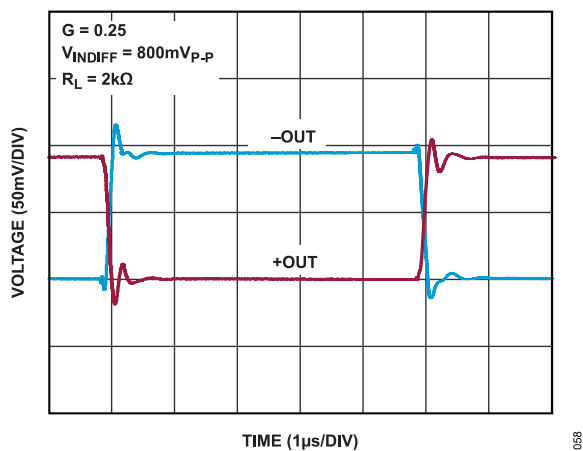


Figure 57. Small Signal Step Response

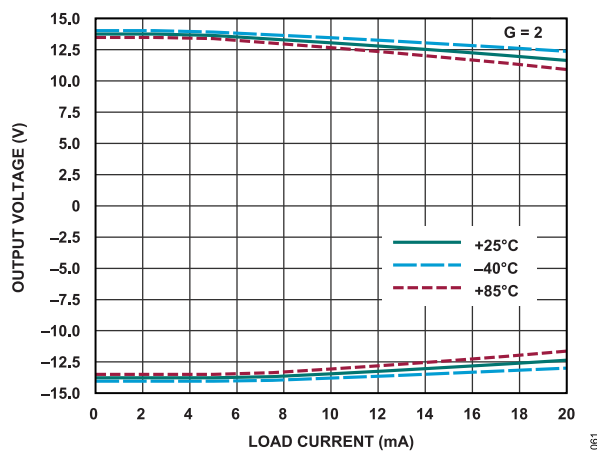


Figure 60. Output Voltage Swing vs. Load Current

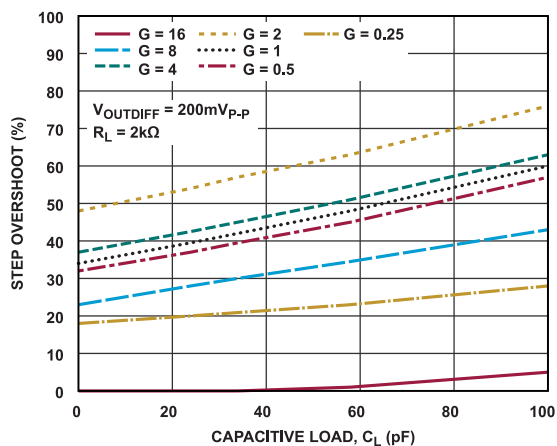


Figure 58. Small Signal Step Overshoot vs. Load Capacitance

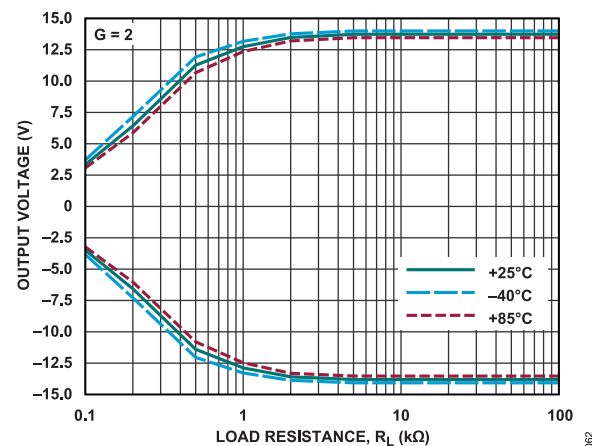


Figure 61. Output Voltage Swing vs. Load Resistance

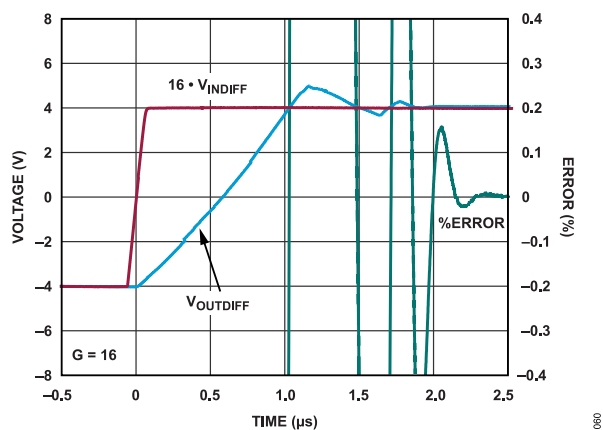
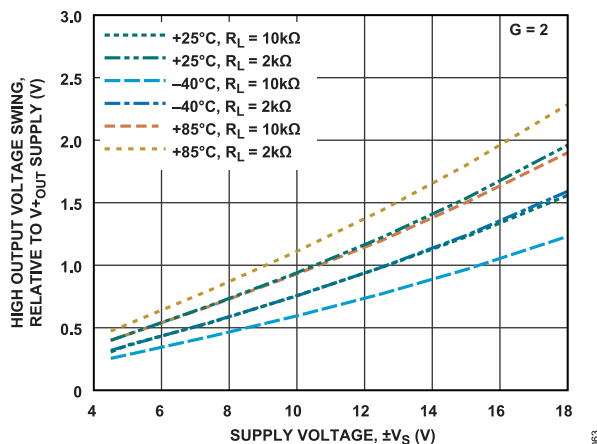
Figure 59. Settling Time to 8 V_{p-p} Output Step

Figure 62. High Output Voltage Swing vs. Supply Voltage

TYPICAL PERFORMANCE CHARACTERISTICS

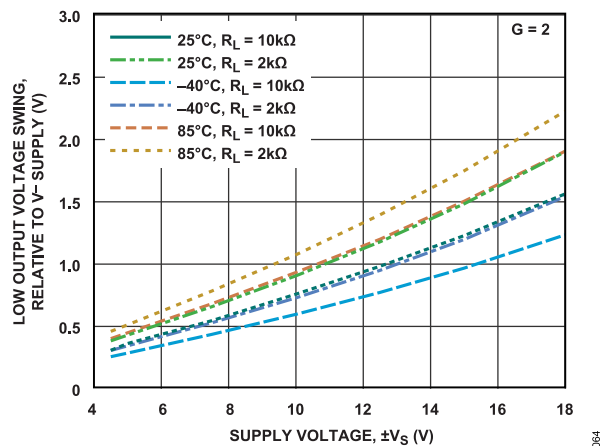


Figure 63. Low Output Voltage Swing vs. Supply Voltage

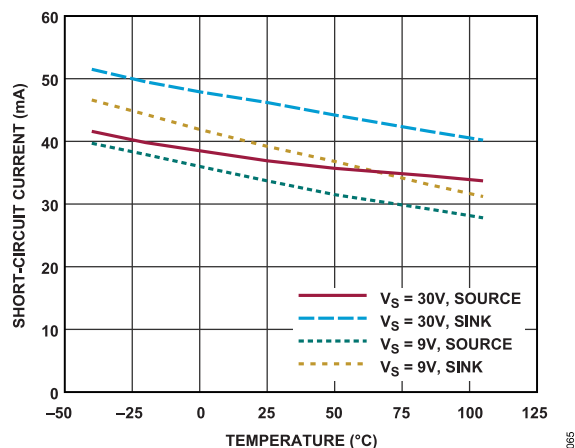


Figure 64. Output Short-Circuit Current vs. Temperature

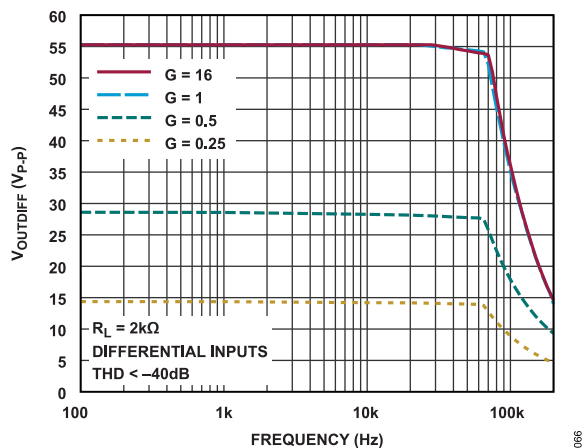


Figure 65. Maximum Undistorted Output Swing vs. Frequency

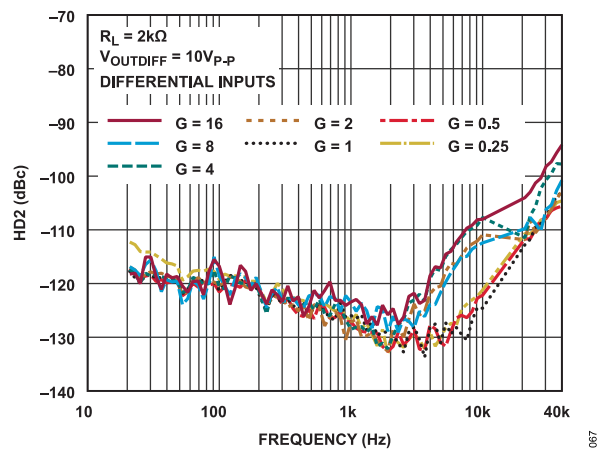


Figure 66. 2nd Harmonic Distortion vs. Frequency

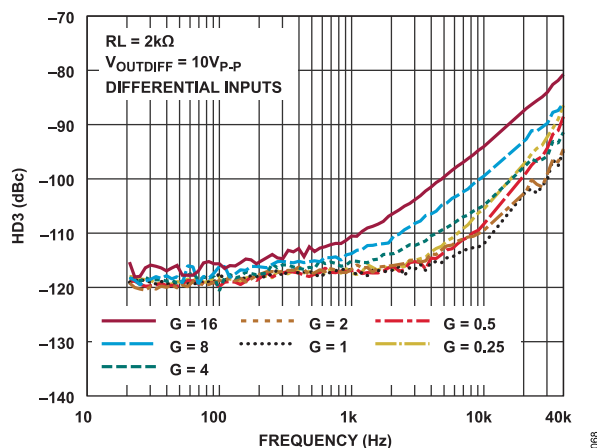


Figure 67. 3rd Harmonic Distortion vs. Frequency

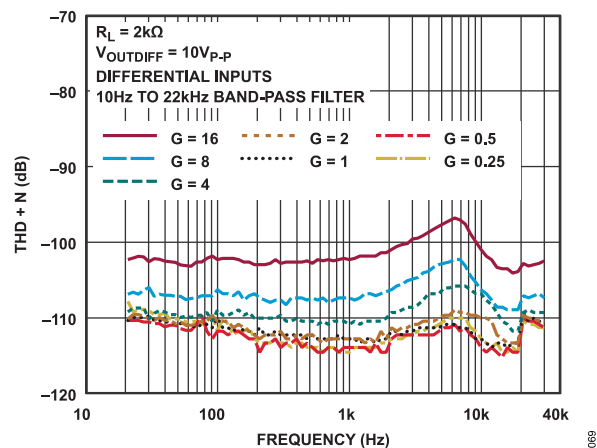


Figure 68. Total Harmonic Distortion + Noise vs. Frequency

TYPICAL PERFORMANCE CHARACTERISTICS

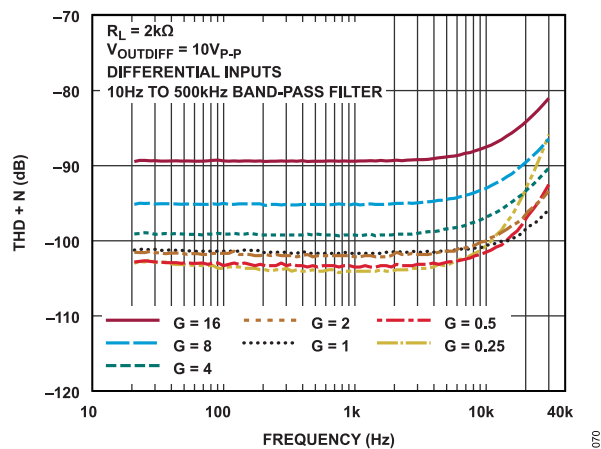


Figure 69. Total Harmonic Distortion + Noise vs. Frequency

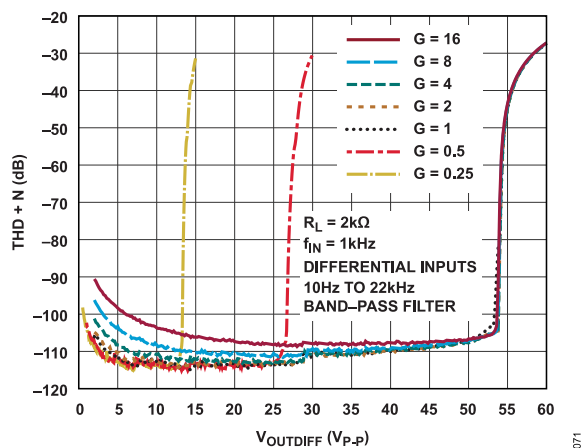


Figure 70. Total Harmonic Distortion + Noise vs. Output Amplitude

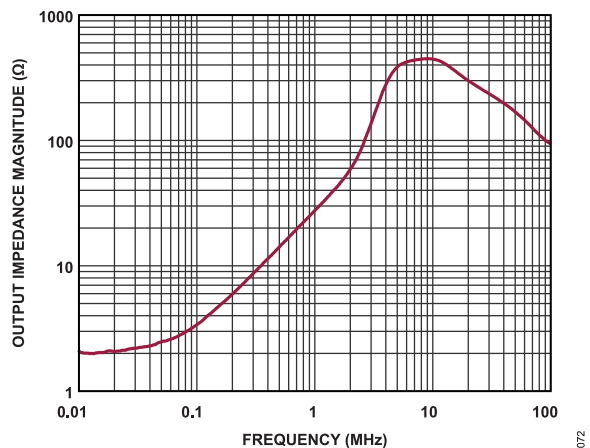


Figure 71. Differential Output Impedance vs. Frequency

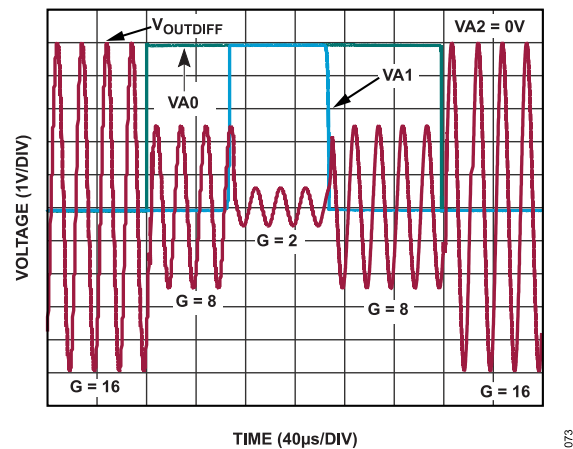


Figure 72. Gain Switching Transient Response

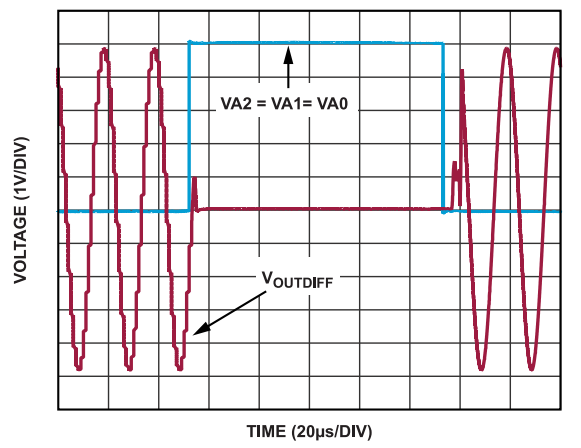


Figure 73. Turn-On and Turn-Off Transient Response

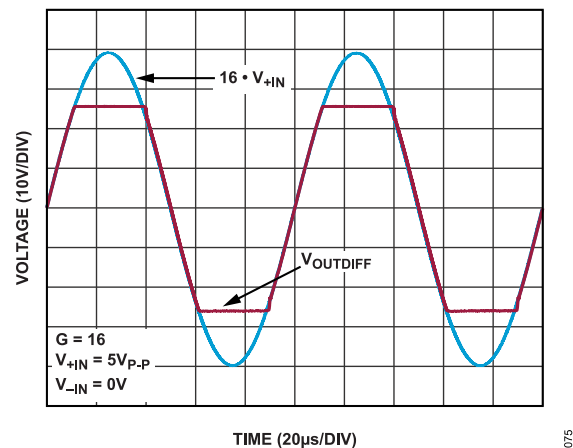


Figure 74. Output Overdrive Recovery

TYPICAL PERFORMANCE CHARACTERISTICS

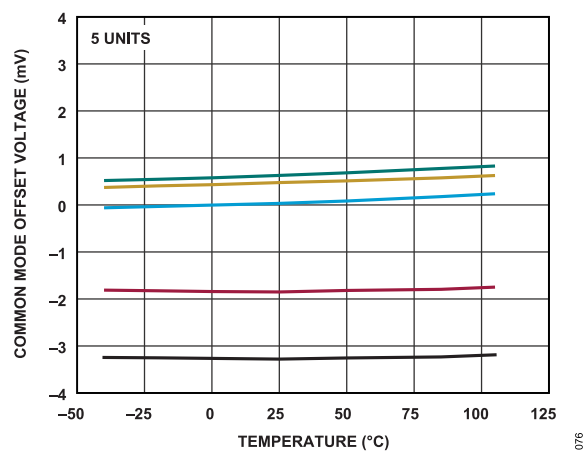


Figure 75. Common Mode Offset Voltage vs. Temperature

THEORY OF OPERATION

FUNCTIONAL DESCRIPTION

The LTC6373 is a monolithic instrumentation amplifier based on the classic 3-op-amp topology, as shown in the Block Diagram of [Figure 76](#). A parallel interface allows users to digitally program gains to one of the seven available settings ($G = 0.25, 0.5, 1, 2, 4, 8$, and 16 V/V) while the 8th state puts the part in shutdown mode (which reduces the current drawn from the supplies to $220 \mu\text{A}$). Gain control is achieved by switching resistors in an internal, precision resistor array (as shown in [Figure 76](#)). Although the LTC6373 has a voltage feedback topology, the gain-bandwidth product increases at higher gain settings because each gain has its own frequency compensation, resulting in increased bandwidth at higher gains and minimum phase variation across all gains.

The LTC6373 is optimized to convert a fully differential or single-ended input signal to a low impedance, balanced differential output suitable for driving high performance, analog-to-digital converters (ADCs). The balanced differential nature of the amplifier provides even-order harmonic distortion cancellation, and low susceptibility to common mode noise (like power supply noise). Load capacitances above 50 pF to ground or 25 pF differentially should be decoupled with 10Ω to 50Ω of series resistance from each output to prevent oscillation or ringing.

Overall, the LTC6373 simplifies signal chain design by offering:

- ▶ High impedance buffering (due to using CMOS technology and the resulting pA input bias current)
- ▶ Signal amplification ($G > 1$) and attenuation ($G < 1$) together in one socket at nearly the same bandwidth
- ▶ Digital gain programming (which enables changing gain settings easily and rapidly)
- ▶ Superior matching specs (due to trimmed, precision internal resistors)
- ▶ The ability to drive ADCs directly (due to attributes such as fully differential outputs, good DC precision, low noise, low distortion, and high bandwidth)
- ▶ Level shifting (achieved by using V_{OCM} pin to independently adjust the output common mode voltage to match it to the desired input level of the next stage of the signal chain).

The LTC6373 accommodates all the above features in a small 12-lead $4 \text{ mm} \times 4 \text{ mm}$ DFN (LFCSP) package, making it an excellent solution for applications where size and packing density are important considerations.

THEORY OF OPERATION

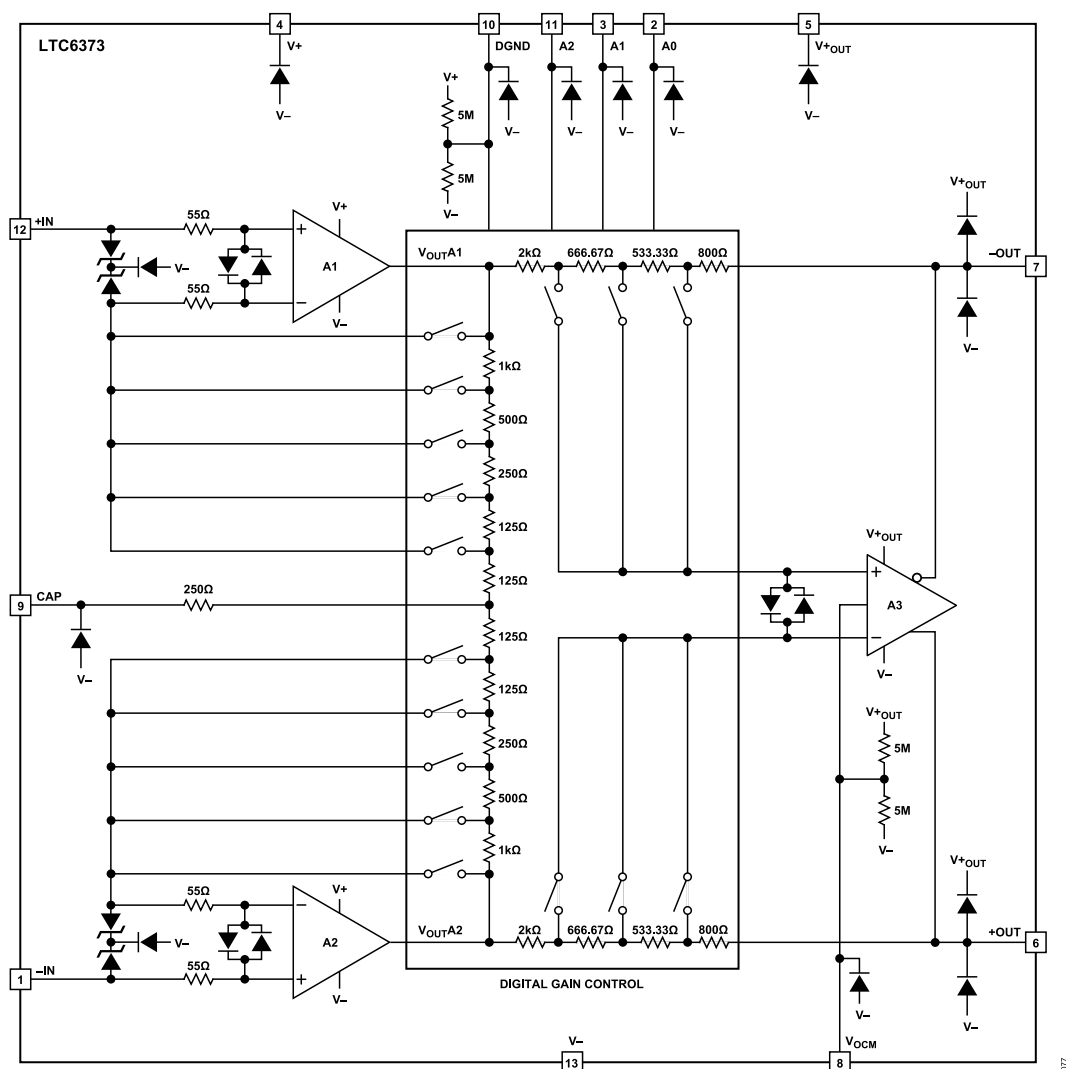


Figure 76. Simplified Block Diagram

APPLICATIONS INFORMATION

GAIN SELECTION

The gain of the LTC6373 can be programmed to its desired setting using a digital interface consisting of a digital reference pin DGND and three parallel gain programming pins A2, A1, and A0. The logic threshold for A2/A1/A0 pins is specified with respect to the voltage on the DGND pin. Any voltage between DGND and DGND + 0.6 V on A2 or A1 or A0 pins will generate a logic low (L) state for that pin; any voltage between DGND + 1.5 V and V⁺ on A2 or A1 or A0 pins will generate a logic high (H) state for that pin. The gain for the LTC6373 is programmed according to the truth table below:

Table 5. Gain Selection Table for LTC6373

A2	A1	A0	G = Gain Setting (V/V)
L	L	L	16
L	L	H	8
L	H	L	4
L	H	H	2
H	L	L	1
H	L	H	0.5
H	H	L	0.25
H	H	H	Shutdown

The permissible voltage range for DGND is between V⁻ and V⁺ - 2.5 V. However, typically DGND is tied to ground (0 V) and A2/A1/A0 pins can be connected to 0 V or 5 V to generate logic low (L) and logic high (H) states, respectively.

If the DGND pin is left floating, an internal resistor divider creates a default voltage approximately halfway between V⁺ and V⁻. Additionally, if A2 or A1 or A0 pins are left floating, internal resistors pull the voltage on each of these pins close to the DGND pin, resulting in a default logic low (L) state for that programming pin. As a result, if A2 and A1 and A0 pins are left floating all at the same time, the LTC6373 will have a gain setting of G = 16. When these pins are left open, care should be taken to control leakage currents at these pins to prevent inadvertently putting the LTC6373 into an undesired gain setting.

Keep in mind that any change in voltages applied to A2 or A1 or A0 pins from logic low to logic high (or vice versa) immediately results in a gain setting change for LTC6373 (transparent mode).

VALID INPUT AND OUTPUT RANGE

Instrumentation amplifiers traditionally specify a valid input common mode range and an output swing range. This however often fails to identify swing limitations associated with internal nodes, as they experience a combination of gained differential signal and common mode signal. Referring to the Simplified Block Diagram of Figure 76, the output swing of amplifiers A1, A2, and A3 as well as the common mode input range of the output differential amplifier A3 impose limitations on the valid operating range. The graphs in Figure 78 to Figure 84 show the maximum input common mode voltage limits where a valid output is produced for each gain setting of LTC6373.

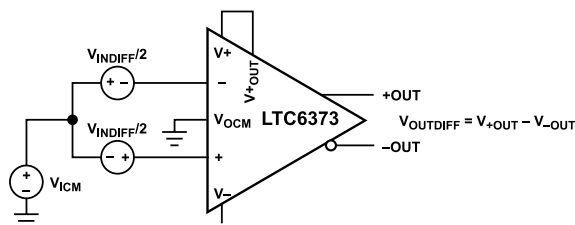


Figure 77. LTC6373 Input Configuration and Differential Output Calculation

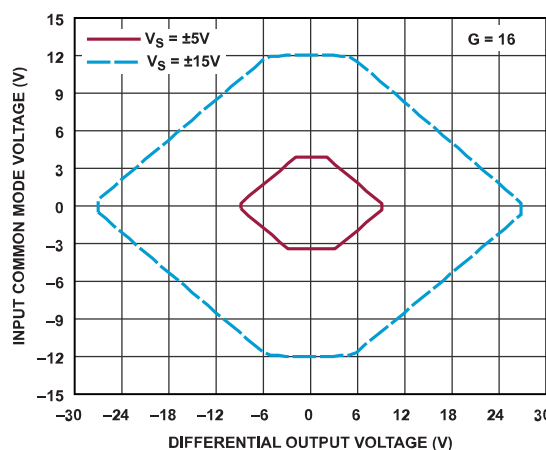


Figure 78. Input Common Mode Range vs. Differential Output Voltage at G = 16 with No Load

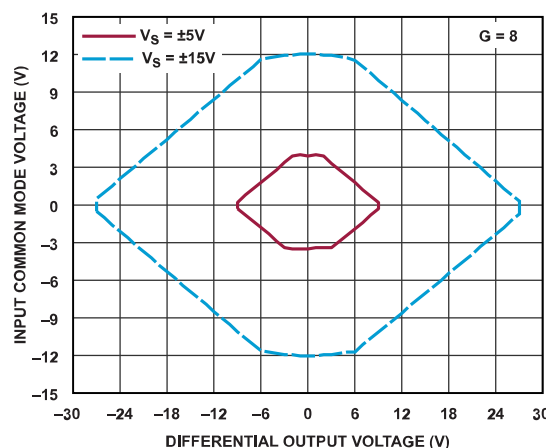


Figure 79. Input Common Mode Range vs. Differential Output Voltage at G = 8 with No Load

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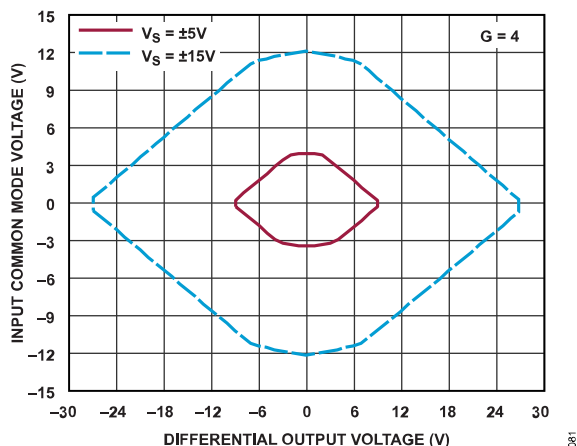


Figure 80. Input Common Mode Range vs. Differential Output Voltage at $G = 4$ with No Load

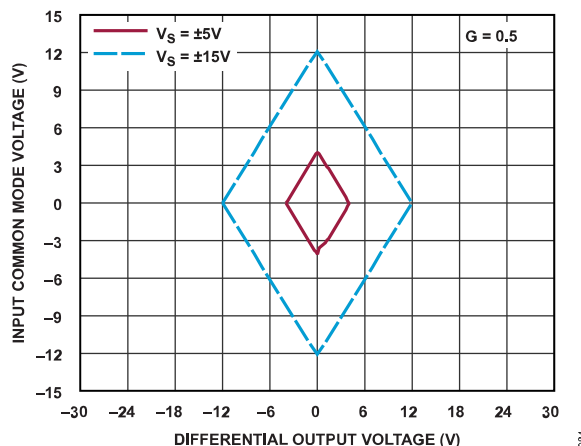


Figure 83. Input Common Mode Range vs. Differential Output Voltage at $G = 0.5$ with No Load

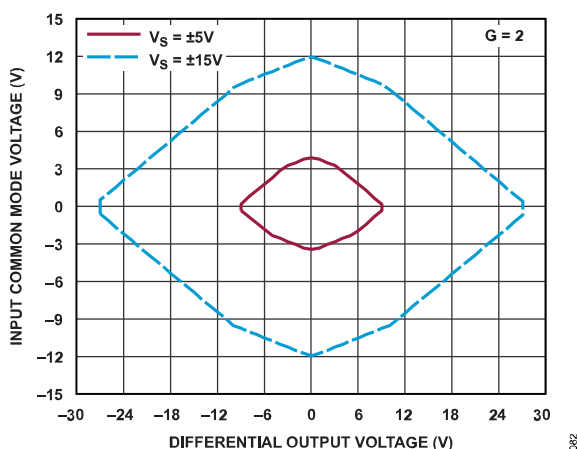


Figure 81. Input Common Mode Range vs. Differential Output Voltage at $G = 2$ with No Load

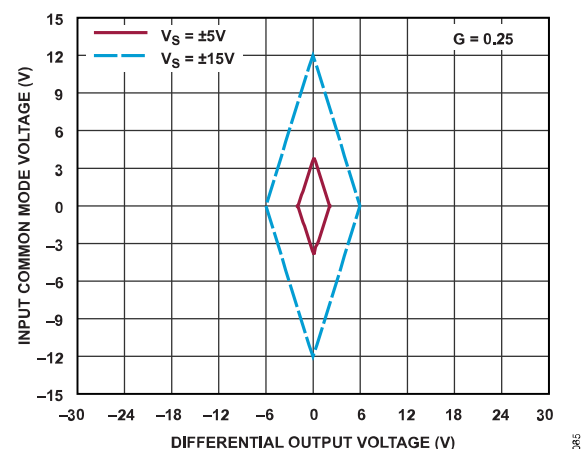


Figure 84. Input Common Mode Range vs. Differential Output Voltage at $G = 0.25$ with No Load

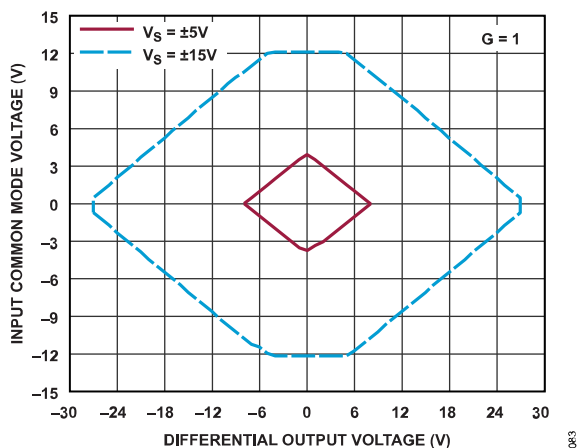


Figure 82. Input Common Mode Range vs. Differential Output Voltage at $G = 1$ with No Load

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DIAMOND PLOT INTERPRETATION

Diamond plots can be used to determine the valid input common mode voltage (V_{ICM}) operating range for instrumentation amplifiers such as LTC6373. The valid region of operation is where all signals, input or output, are not clipped.

Plots in Figure 78 to Figure 84 show the input common mode voltage (V_{ICM}) range allowed for a given differential output voltage ($V_{OUTDIFF}$), under various combinations of gain (G) and supply (V_S) settings. In each plot, the output stage positive supply pin V_{+OUT} is tied to the main positive supply pin V^+ , $V_{OCM} = 0$ V (mid-rail) and there is no load.

To identify the valid V_{ICM} range for a specific application: First, identify the gain and supply conditions that the LTC6373 will be operated under. Then, identify the range of valid differential output voltages ($V_{OUTDIFF}$) desired. For example, this could be the full-scale signal that is optimal for the subsequent ADC's SNR.

This combination of settings and output range implies a specific differential input signal (V_{INDIFF}) range, since $V_{INDIFF} = V_{OUTDIFF}/G$.

While the input signal's V_{INDIFF} is fixed when specific $V_{OUTDIFF}$ and G are chosen, the input signal's common mode voltage V_{ICM} is not, because the same V_{INDIFF} can be superimposed on many different V_{ICM} values.

The valid V_{ICM} range can be set by the swing limits on $+IN$ and/or $-IN$, since V_{ICM} is the average of $+IN$ and $-IN$. It can also be set by internal node swing limits, since the internal nodes are also operating with common mode voltage V_{ICM} , and these nodes must also be able to swing enough away from V_{ICM} to produce the gained-up output.

On a diamond plot, this valid region of operation for V_{ICM} for a specific output $V_{OUTDIFF}$ is indicated by the portion of the vertical line going straight up from $V_{OUTDIFF}$ that falls inside the diamond borders, as shown in Figure 85.

If the part's input common mode voltage is within the V_{ICM} borders of the diamond, there should be no problems with clipping. If the differential input signal is shifted by a V_{ICM} value that is outside of the diamond, either $+IN$ or $-IN$ (or internal nodes) will be clipped, or the output itself will hit the rails, and thus result in a clipped output.

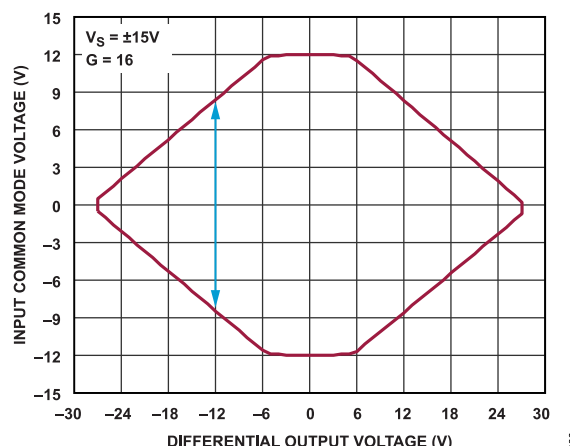


Figure 85. The Blue Arrow Indicates the Range of Valid V_{ICM} Values for $V_{OUTDIFF} = -12$ V, Where No Signals are Clipped, for the $V_S = \pm 15$ V, $G = 16$ Case

The following example shows how a diamond plot point is determined. For the specific case of $V_{OUTDIFF} = -12$ V as shown in Figure 85, the upper limit of V_{ICM} is 8 V, and the lower limit is -8 V.

For $V_{ICM} = 8$ V, if the gained-up input (aka output) is -12 V, the maximum negative internal node swing is 6 V above V_{ICM} . Referenced to ground, this internal node reaches 8 V + 6 V = 14 V, which is roughly the output high limit of LTC6373 with ± 15 V supplies. If V_{ICM} were any higher than 8 V, the internal node would run into the output high limit, and the output would clip.

For $V_{ICM} = -8$ V, with -12 V output, the minimum positive internal node swing is -6 V below V_{ICM} . Referenced to ground, this internal node can hit a minimum of -6 V + (-8 V) = -14 V, which is roughly the output low limit of LTC6373 with ± 15 V supplies. If V_{ICM} were any lower than -8 V, this internal node would run into the output low limit, and the output would clip.

OUTPUT COMMON MODE AND V_{OCM} PIN

The output common mode voltage is defined as the average of the two outputs:

$$V_{OUTCM} = (V_{+OUT} + V_{-OUT})/2 = V_{OCM}$$

As the equation shows, the output common mode voltage is independent of the input common mode voltage, and is instead determined by the voltage on the V_{OCM} pin, by means of an internal common mode feedback loop. If the V_{OCM} pin is left floating, an internal resistor divider creates a default voltage approximately halfway between V_{+OUT} and V^- . The V_{OCM} pin can be overdriven to another voltage if desired for greater accuracy or flexibility. For example, when driving an ADC, if the ADC makes a reference available for setting the common mode voltage, it can be directly tied to the V_{OCM} pin, as long as the ADC is capable of driving the 2.3 M Ω input resistance presented by the V_{OCM} pin. The Electrical Characteristics table specifies the valid range that can be applied to the V_{OCM} pin (V_{OUTCMR}).

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INPUT PIN PROTECTION

To prevent damage, the LTC6373 has a comprehensive protection scheme, especially on the input pins, as illustrated in the Simplified Block Diagram of Figure 76. The input current applied to the LTC6373's input pins should be kept under ± 10 mA. To achieve additional input protection, external series resistors and/or low leakage clamp diodes should be used.

REDUCING BOARD-RELATED LEAKAGE EFFECTS

Leakage currents can have a significant impact on system accuracy, particularly in high temperature and high voltage applications. Quality insulation materials should be used, and insulating surfaces should be cleaned to remove fluxes and other residues. For humid environments, surface coating may be necessary to provide a moisture barrier.

Leakage into the input pins reacts with the source resistance, creating an error directly at the input. As shown in Figure 86, this leakage can be minimized by enclosing the input connections with guard rings operated at a potential very close to that of the input pins. For the lowest leakage, amplifiers can be used to drive the guard rings. These buffers must have very low input bias current since that current will now be a leakage current.

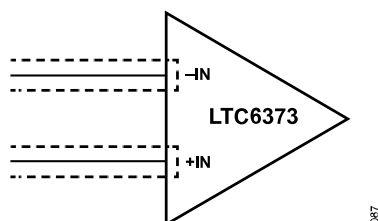


Figure 86. Guard Rings Can Be Used to Minimize Leakage into the Input Pins

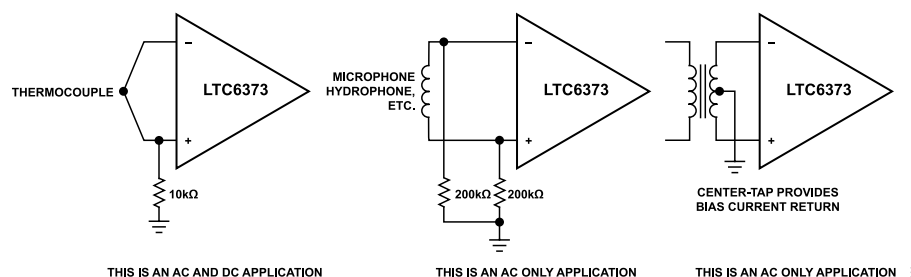


Figure 87. Providing an Input Common Mode Current Path

INPUT BIAS CURRENT RETURN PATH

The low input bias current (25 pA max) and high input impedance (5000 G Ω) of the LTC6373 allow the use of high impedance sources without introducing additional offset voltage errors, even when the full common mode range is required. However, a DC path must be provided for the input bias currents of both inputs when a purely differential signal is being amplified. Without this path, the inputs will float to either rail and exceed the input voltage range of the LTC6373, resulting in a saturated input amplifier. Figure 87 shows three examples of an input bias current path. The first example is of a purely differential signal source with a 10 k Ω input current path to ground. Since the impedance of the signal source is low, only one resistor is needed. Two matching resistors are needed for higher impedance signal sources as shown in the second example. Balancing the input impedance improves both DC and AC common mode rejection as well as DC offset. The need for input resistors is eliminated if a center tap is present as shown in the third example.

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RF INTERFERENCE

In many industrial and data acquisition applications, the LTC6373 will be used to process small signals accurately in the presence of large common mode voltages or high levels of noise. Typically, the sources of these very small signals (on the order of microvolts or millivolts) are sensors that can be a significant distance from the signal conditioning circuit. Although these sensors may be connected to signal conditioning circuitry using shielded or unshielded twisted-pair cabling, the cabling may act as an antenna, conveying very high frequency interference directly into the input stage of the LTC6373.

The amplitude and frequency of the interference can have an adverse effect on an instrumentation amplifier's input stage by causing an unwanted DC shift in the amplifier's input offset voltage. This well known effect is called RFI rectification and is produced when out-of-band interference is coupled (inductively, capacitively, or via radiation) and rectified by the instrumentation amplifier's input transistors. These transistors act as high frequency signal detectors, in the same way diodes were used as RF envelope detectors in early radio designs. Regardless of the type of interference or the method by which it is coupled into the circuit, an out-of-band error signal appears in series with the instrumentation amplifier's inputs.

To help minimize this effect, high frequency signals can be filtered with a low pass RC network placed at the input of the LTC6373, as illustrated in Figure 88.

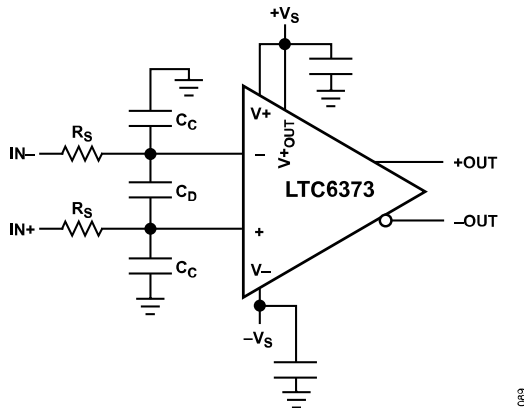


Figure 88. Adding a Simple External RC Filter at the Inputs of the LTC6373 Is Effective in Suppressing RF Interference.

The filter limits the input signal bandwidth according to the following formulas:

$$\text{FilterFreq}_{\text{DIFF}} = 1/[2 \times \pi \times R_S \times (C_C + 2C_D)]$$

$$\text{FilterFreq}_{\text{CM}} = 1/[2 \times \pi \times R_S \times C_C]$$

Setting the filter frequencies requires knowledge of the frequency (or frequencies) of the RF interference. Once the interference

frequency is known, the common mode filter frequency can be set (low enough to filter out the interference frequency) followed by the differential mode filter frequency. To avoid any possibility of inadvertently affecting the differential signal of interest, set the common mode filter frequency an order of magnitude (or more) higher than the differential mode filter frequency. Set the common mode filter frequency such that it does not degrade the LTC6373's inherent AC CMRR. To avoid any possibility of common mode to differential mode signal conversion, match the common mode filter frequencies (on positive and negative inputs of LTC6373) to 1% or better. Then the differential mode filter frequency can be set for the bandwidth of the signal to be processed in the application. Setting the differential mode filter frequency close to the sensor's bandwidth also minimizes any noise pickup along the leads. If the sensor is an RTD or a resistive strain gauge in close proximity to the LTC6373, then the series resistors R_S can be omitted. As an example, if the bandwidth of the signal of interest is 100 kHz whereas the interference frequency is 10 MHz and above, an appropriate choice for differential mode filter ($\text{FilterFreq}_{\text{DIFF}}$) and common mode filter ($\text{FilterFreq}_{\text{CM}}$) frequencies could be 200 kHz/4 MHz. Assuming R_S is chosen to be 1 k Ω , using the formula provided earlier in this section results in $C_C = 39$ pF and $C_D = 390$ pF.

ERROR BUDGET ANALYSIS

Figure 89 shows the LTC6373 in a typical application to buffer and amplify the differential output of a bridge transducer. The LTC6373 is programmed to a gain of 8 V/V in this example and amplifies a differential, full-scale (FS) voltage of 100 mV = 0.1 V at transducer's output (or LTC6373's input). Table 6 shows the error budget in this application, listing various error sources in parts per million (ppm) normalized to full-scale voltage (0.1 V) and across the temperature range of 25°C to 85°C. The LTC6373 achieves superior performance compared to all other monolithic programmable-gain instrumentation amplifiers (PGIA) in the market, enabling more accurate measurements.

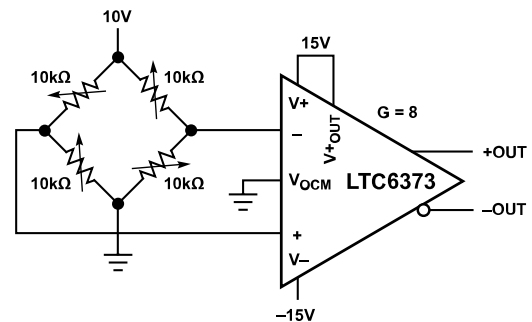


Figure 89. Precision Bridge Amplifier

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Table 6. Error Budget Analysis

Error Source	Calculation		Error, ppm of Input Full Scale (FS)	
	LTC6373 (G = 8)	Closest Competitor PGIA (G = 8)	LTC6373 (G = 8)	Closest Competitor PGIA (G = 8)
Absolute Accuracy at $T_A = 25^\circ\text{C}$				
Gain Error	0.015% FS	0.05% FS	150	500
Offset Voltage (RTI)	$(104\ \mu\text{V})/0.1\ \text{V}$	$(1500\ \mu\text{V})/0.1\ \text{V}$	1040	15000
Input Offset Current	$[(25\ \text{pA})(10\ \text{k}\Omega)/2]/0.1\ \text{V}$	$[(100\ \text{pA})(10\ \text{k}\Omega)/2]/0.1\ \text{V}$	1	5
CMRR	$[(5\ \text{V})/(100\ \text{dB})]/0.1\ \text{V}$	$[(5\ \text{V})/(95\ \text{dB})]/0.1\ \text{V}$	500	889
Total Accuracy Error			1691	16394
Temperature Drift to 85°C				
Gain Drift	$(1\ \text{ppm}/^\circ\text{C})(60^\circ\text{C})$	$(10\ \text{ppm}/^\circ\text{C})(60^\circ\text{C})$	60	600
Offset Voltage Drift (RTI)	$[(1.8\ \mu\text{V}/^\circ\text{C})(60^\circ\text{C})]/0.1\ \text{V}$	$[(6\ \mu\text{V}/^\circ\text{C})(60^\circ\text{C})]/0.1\ \text{V}$	1080	3600
Total Drift Error			1140	4200
Resolution				
Gain Nonlinearity	3 ppm	20 ppm	3	20
Typ 0.1 Hz to 10 Hz Input Voltage Noise	$(1.2\ \mu\text{V}_{\text{P-P}})/0.1\ \text{V}$	$(1\ \mu\text{V}_{\text{P-P}})/0.1\ \text{V}$	12	10
Total Resolution Error			15	30
Grand Total Error			2846	20624

DYNAMIC POWER CONSUMPTION CALCULATION

As shown in the Simplified Block Diagram of Figure 76, the LTC6373 has three internal chains of gain setting resistors. To achieve a low wideband noise for the LTC6373, a relatively small value, 4 k Ω , has been chosen for the total resistance of each chain. The voltages across the three chains are:

1. V_{OUTA1} to $-\text{OUT}$
2. V_{OUTA2} to $+\text{OUT}$
3. V_{OUTA1} to V_{OUTA2}

Each of these voltages is imposed across what is effectively one 4 k Ω resistor, establishing currents in them. These three currents are independent of each other and the part's quiescent supply current (I_S), and all of them are drawn from the supplies.

For example, assume LTC6373 is being used with $\pm 15\ \text{V}$ supplies (i.e., $V^+ = V_{\text{OUT}}^+ = 15\ \text{V}$, $V^- = -15\ \text{V}$), $V_{\text{OCM}} = 0\ \text{V}$, $G = 2$, and has input voltages of $+\text{IN} = 3\ \text{V}$ and $-\text{IN} = -3\ \text{V}$ (i.e., $V_{\text{ICM}} = 0\ \text{V}$, $V_{\text{INDIFF}} = 6\ \text{V}$). The resulting output voltage is $V_{\text{OUTDIFF}} = 2 \times V_{\text{INDIFF}} = 12\ \text{V}$. Since $V_{\text{OUTCM}} = V_{\text{OCM}} = 0\ \text{V}$, this implies that the value of LTC6373's output voltages are $+\text{OUT} = 6\ \text{V}$, $-\text{OUT} = -6\ \text{V}$.

Since the gain is applied in the A1 and A2 amplifiers, the output voltages of these internal amplifiers are $V_{\text{OUTA1}} = +6\ \text{V}$ and $V_{\text{OUTA2}} = -6\ \text{V}$, respectively.

Thus, the voltages and currents in each 4 k Ω resistor chain are:

$$I_1 = [(V_{\text{OUTA1}}) - (-\text{OUT})]/4\ \text{k}\Omega = [6\ \text{V} - (-6\ \text{V})]/4\ \text{k}\Omega = 3\ \text{mA}$$

$$I_2 = [(+\text{OUT}) - (V_{\text{OUTA2}})]/4\ \text{k}\Omega = [6\ \text{V} - (-6\ \text{V})]/4\ \text{k}\Omega = 3\ \text{mA}$$

$$I_3 = [(V_{\text{OUTA1}}) - (V_{\text{OUTA2}})]/4\ \text{k}\Omega = [6\ \text{V} - (-6\ \text{V})]/4\ \text{k}\Omega = 3\ \text{mA}$$

Therefore, the total supply current is:

$$I_{\text{TOTAL}} = I_S + I_1 + I_2 + I_3 = 4.4\ \text{mA} + 3 \times 3\ \text{mA} = 13.4\ \text{mA}$$

In case the output pins ($+\text{OUT}$, $-\text{OUT}$) of the LTC6373 connect to resistive loads, the currents provided by the LTC6373 to these loads should also be added to the calculations above.

BOARD LAYOUT AND BYPASS CAPACITORS

It is recommended that high quality 0.1 μF ceramic bypass capacitors be placed directly between the V^+ pin and the V^- pin (exposed pad), between V^+ and ground plane, and between V^- and ground plane with minimal routing. In applications where V_{OUT}^+ pin is not directly connected to V^+ , it is recommended that additional high quality 0.1 μF ceramic capacitors be used to bypass V_{OUT}^+ to ground and V_{OUT}^+ to V^- , again with minimal routing. Small geometry (e.g., 0603) surface mount ceramic capacitors have a much higher self-resonant frequency than leaded capacitors, and perform best with the LTC6373.

Always keep in mind the differential nature of the LTC6373. At the inputs, keep any (intended or parasitic) resistance and capacitance as balanced and symmetric as possible to preserve AC CMRR performance of the amplifier. Apply the same practice at the output, because it is equally critical that the load impedances seen by both outputs (intended or parasitic) be as balanced and symmetric as possible. This will help preserve the balanced operation of the LTC6373 that minimizes the generation of even-order harmonics and maximizes the rejection of common mode noise and signals.

To minimize thermocouple induced errors, further attention must be given to board layout and component selection. It is good practice to minimize the number of junctions in the LTC6373's input signal paths and avoid connectors, sockets, switches, and relays whenever possible. If such components are required, they should be selected for low thermal EMF characteristics. Furthermore, the number, type, and layout of junctions should be matched for both

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inputs with respect to thermal gradients on the circuit board. Doing so may involve deliberately introducing dummy junctions to offset unavoidable junctions.

The V_{OCM} pin should be bypassed to the ground plane with a high quality 0.1 μ F ceramic capacitor. This will prevent common mode signals and noise on this pin from being inadvertently converted to differential signals and noise by impedance mismatches internally to the IC. Additionally, the CAP pin should be bypassed to the ground plane with a high quality 180 pF ceramic capacitor to ensure proper operation of LTC6373 across its different gain settings.

To prevent coupling noise onto LTC6373, shield fast switching digital signals where they are in proximity of analog signals on the board.

DRIVING HIGH PRECISION ADCS

The LTC6373 makes an excellent PGIA for use in data acquisition systems. Attributes such as fully differential outputs, good DC precision, low noise, low distortion, and high bandwidth enable LTC6373 to drive ADCs directly in many signal conditioning applications. The recommended list of precision SAR ADCs for use with the LTC6373 is shown in Table 7. The circuit in Figure 90 shows an example

of the LTC6373 driving a precision ADC such as the AD4020 (a 20-bit, 1.8 Msps, SAR ADC) or AD7134 (a 24-bit, 1.5 Msps, Continuous-Time, Σ - Δ ADC). The LTC6373 is DC-coupled on the input and the output, which eliminates the need for a transformer to drive the ADC. The LTC6373 gain is programmed to its desired setting using A2/A1/A0 pins, as previously described in the Gain Selection section of this data sheet. In the example of Figure 90, the LTC6373 is being used in a differential input to differential output configuration with dual supplies of ± 15 V. It can also be used in a single-ended input to differential output configuration.

The V_{OCM} pin is biased to $V_{REF}/2$ (which is provided directly by the ADC in some products). This achieves level shifting of the outputs of the LTC6373 to match the desired input common mode of the ADC. In Figure 90, each of the LTC6373 outputs swings between 0 V and V_{REF} (opposite in phase), thus providing $2 \times V_{REF}$ peak-to-peak differential signal to the ADC inputs. In some cases, an RC network between the LTC6373 outputs and the ADC inputs is required providing a single-pole, low-pass filter to help reduce nonlinear charge kickback due to ADC input switching as well as limiting the broadband noise.

Table 7. Recommended SAR ADCs

Resolution (Bits)	Product	Max Throughput (Msps)	Power @ Max Throughput (mW)	Typical SNR (dB)
20	AD4020	1.8	15	100.5
	LTC2378-20	1	21	104
18	AD4003	2	16	100.5
	LTC2379-18	1.6	18	101.2
16	AD4001	2	16	96.2
	LTC2380-16	2	19	96.2

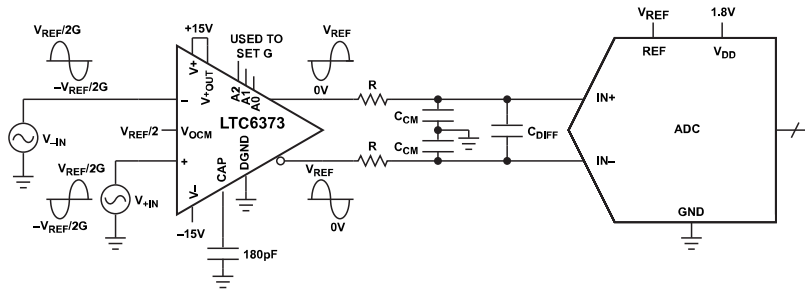


Figure 90. LTC6373 Driving Precision ADC (SAR ADC: Refer to Table 7; Σ - Δ ADC: AD7134)

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As a more specific example, [Figure 91](#) and [Figure 92](#) show typical Signal-to-Noise Ratio (SNR) and Total Harmonic Distortion (THD) of the LTC6373 driving the [AD4020](#) SAR ADC (with high-Z mode enabled) at a near full-scale signal for various ADC throughputs. The recommended RC filter values used in [Figure 90](#) for optimum performance at each throughput are listed in [Table 8](#), as well as the selected reference voltage (V_{REF}).

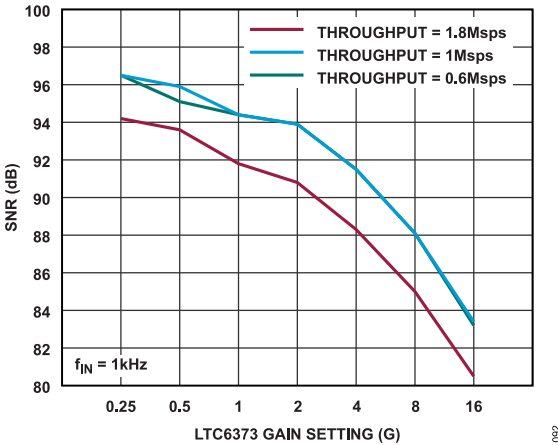


Figure 91. SNR for LTC6373 Driving AD4020

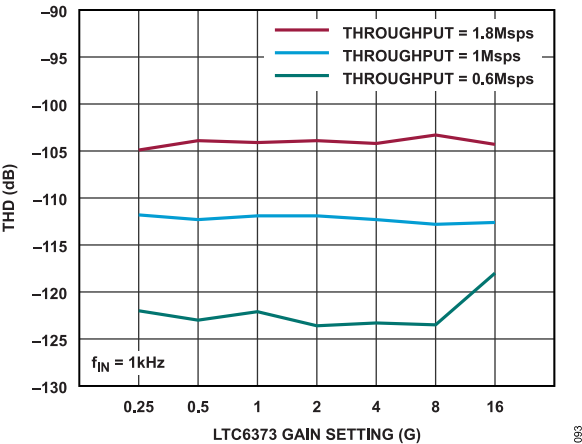


Figure 92. THD for LTC6373 Driving AD4020

Table 8. RC Filter Selection for LTC6373 Driving AD4020 (at Various Throughputs)

ADC	Throughput (MSPS)	V_{REF} (V)	Signal Level at LTC6373			C_{DIFF} (pF)	Typical SNR (dB)	Typical THD (dB)
			Outputs = ADC Inputs (V_{P-P})	R (Ω)	C_{CM} (pF)			
AD4020	1.8	5	10	442	180	Open	See Figure 91	See Figure 92
	1	5	10	887	180	Open	See Figure 91	See Figure 92
	0.6	5	10	887	180	Open	See Figure 91	See Figure 92

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Table 9 lists the typical SNR and THD achieved when the ADC used in Figure 90 is AD7134 Σ - Δ ADC being driven directly (with no RC filter in between) by the LTC6373 at a near full-scale signal.

In some applications, it might be beneficial to use a separate amplifier/ADC driver between the LTC6373 and the precision ADC to ease the settling requirements on the LTC6373 and improve the linearity and THD performance of the signal chain. An implementation of such signal chain can be achieved by using the ADAQ4003, a precision data acquisition μ Module which integrates multiple signal conditioning and processing blocks inside a single package. These blocks include a fully differential ADC driver, a

stable reference buffer, an 18-bit, 2 Msps, SAR ADC, as well as critical passive components necessary for optimum performance. This μ Module achieves 4X footprint reduction by itself (compared to discrete solution) without sacrificing any performance.

The ADAQ4003 offers pin-selectable gain or attenuation options, giving the user the flexibility to match to their input signal range. This is showcased in Figure 93–Figure 101 as LTC6373 is directly driving the ADAQ4003 at its 3 different gain options, in each case providing the signal amplitude necessary to utilize the maximum $2 \times V_{REF}$ peak-to-peak differential signal range of the ADC inside the ADAQ4003 μ Module.

Table 9. SNR and THD Results for LTC6373 Directly Driving AD7134 (at 250 ksp/s)

ADC	LTC6373 Gain Setting (G)	V_{REF} (V)	Signal Level at LTC6373 Outputs = ADC Inputs ($V_{P,P}$)	R (Ω)	C_{CM} (pF)	C_{DIFF} (pF)	f_{IN} (kHz)	Typical SNR (dB)	Typical THD (dB)
AD7134	0.25	4.096	8.192	0	Open	Open	1	108.4	–124
							20	107.7	–97
	1	4.096	8.192	0	Open	Open	1	107.2	–121
							20	106.9	–100
	16	4.096	8.192	0	Open	Open	1	94.3	–112
							20	94.3	–93

Table 10. Details for LTC6373 Driving ADAQ4003 at 3 Different Gain Options and Signal Amplitudes

ADAQ4003 Gain	V_{REF} (V)	Signal Level at LTC6373 Outputs = ADAQ4003 Inputs ($V_{P,P}$)	Circuit Configuration	Typical SNR (dB)	Typical THD (dB)
0.454	5	22	See Figure 93	See Figure 94	See Figure 95
0.9	5	11	See Figure 96	See Figure 97	See Figure 98
1.9	5	5.2	See Figure 99	See Figure 100	See Figure 101

APPLICATIONS INFORMATION

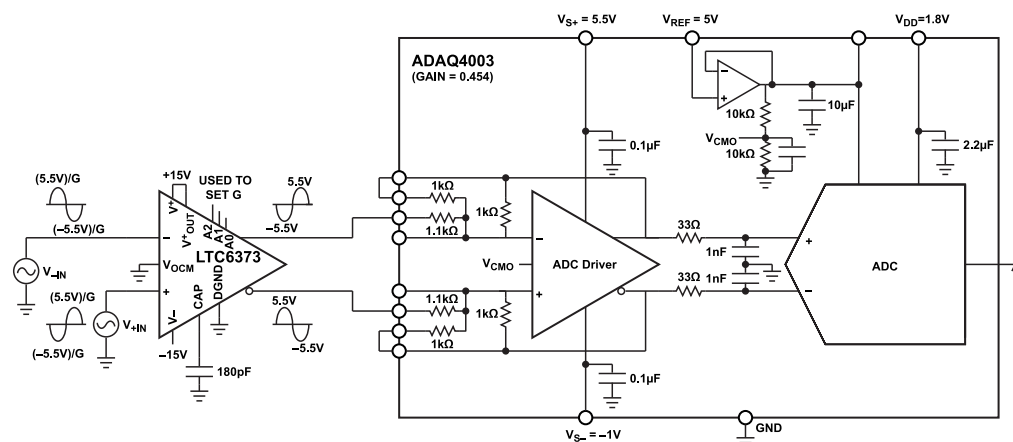


Figure 93. LTC6373 Driving ADAQ4003 (Gain = 0.454)

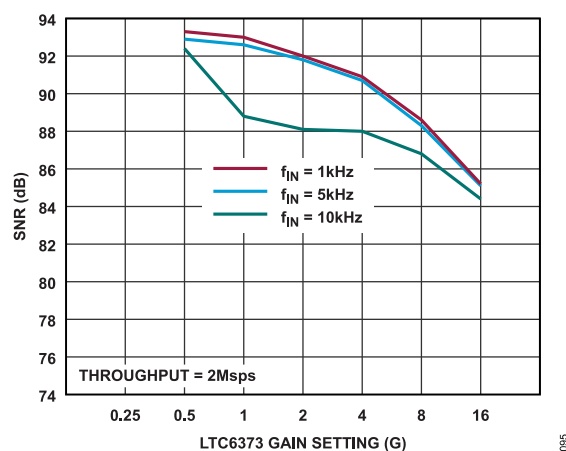


Figure 94. SNR for LTC6373 Driving ADAQ4003 (Gain = 0.454)

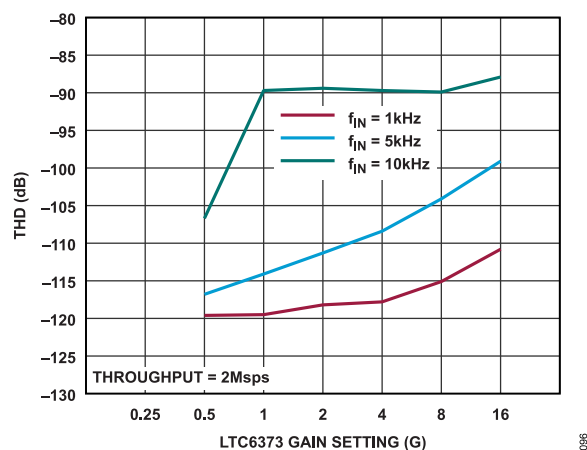


Figure 95. THD for LTC6373 Driving ADAQ4003 (Gain = 0.454)

APPLICATIONS INFORMATION

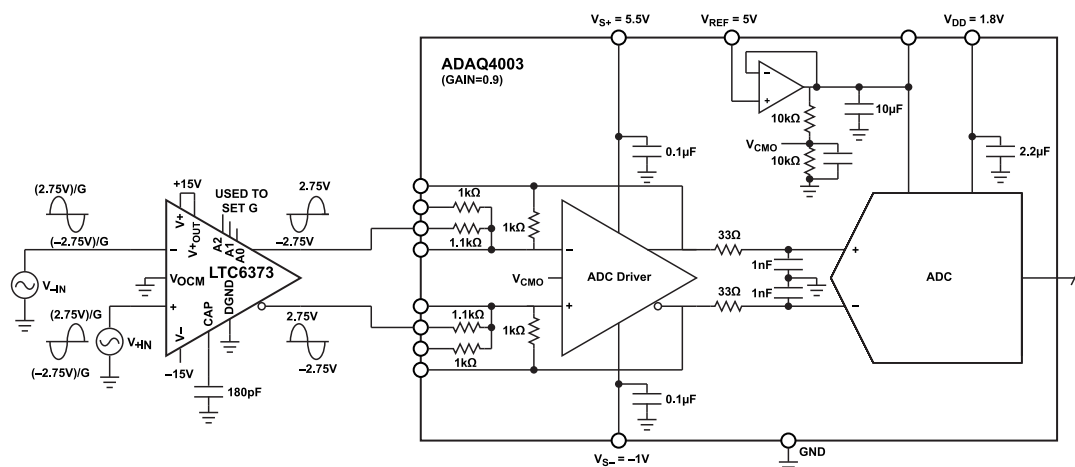


Figure 96. LTC6373 Driving ADAQ4003 (Gain = 0.9)

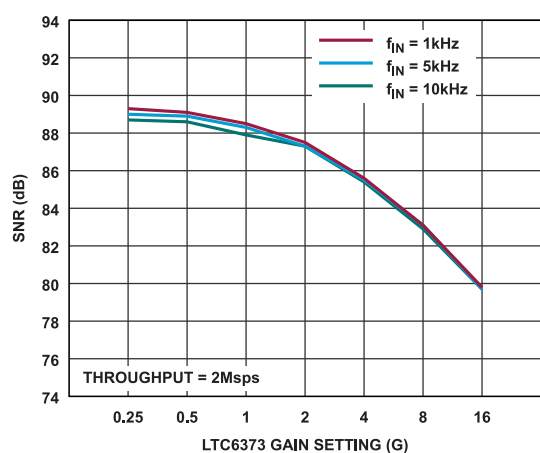


Figure 97. SNR for LTC6373 Driving ADAQ4003 (Gain = 0.9)

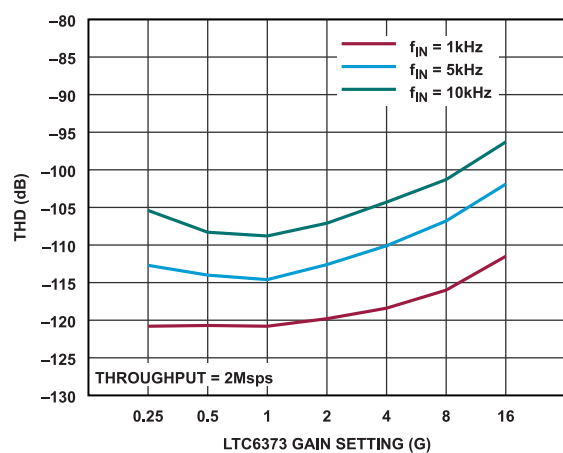


Figure 98. THD for LTC6373 Driving ADAQ4003 (Gain = 0.9)

APPLICATIONS INFORMATION

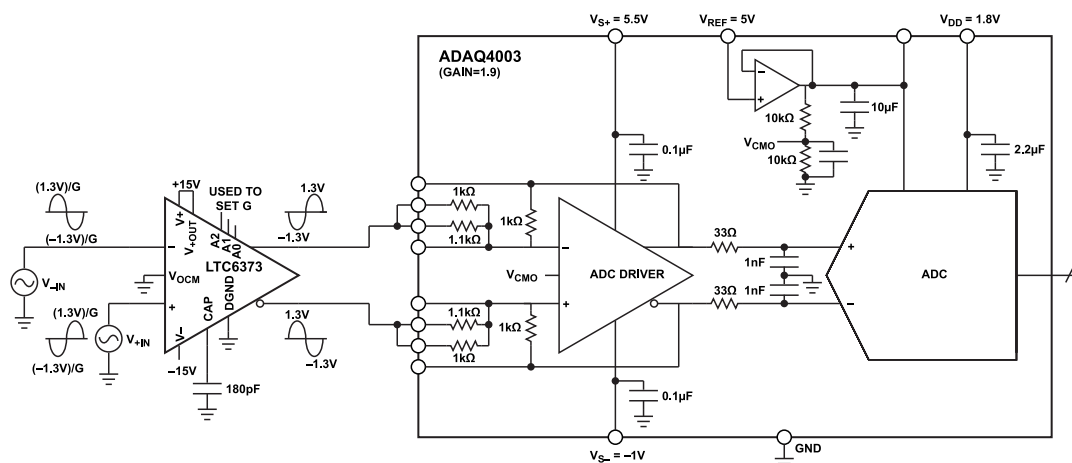


Figure 99. LTC6373 Driving ADAQ4003 (Gain = 1.9)

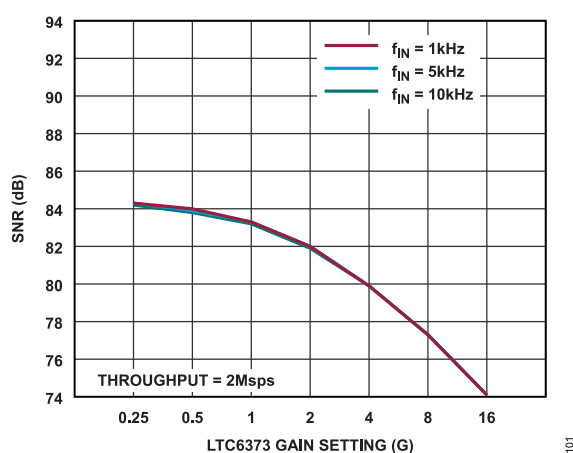


Figure 100. SNR for LTC6373 Driving ADAQ4003 (Gain = 1.9)

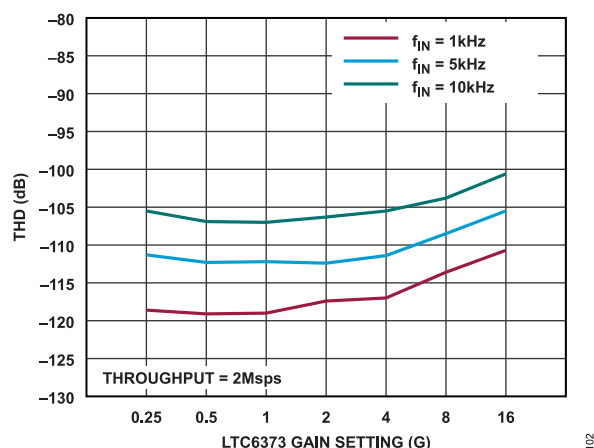


Figure 101. THD for LTC6373 Driving ADAQ4003 (Gain = 1.9)

As another data acquisition system example, the circuit of [Figure 102](#) shows the LTC6373 driving the AD7768-1 (a 24-bit, 256 ksp/s, $\Sigma\Delta$ ADC) through the ADA4945-1 (a high speed, fully differential ADC driver). The ADC driver in this circuit has been configured with

a closed-loop gain of 1.3 V/V (by using matched discrete resistors) and once again the LTC6373 in conjunction with the ADA4945-1 provide the maximum $2 \times V_{REF}$ peak-to-peak differential signal range needed at the AD7768-1 inputs. More details about this circuit can be found in [Table 11](#) and the typical SNR and THD achieved by this signal chain are illustrated in [Figure 103](#) and [Figure 104](#).

Table 11. Details for LTC6373 Driving AD7768-1 Through ADA4945-1

LTC6373 Gain Setting (G)	SNR (dB)
0.25	106.2
0.5	106.0
1	105.5
2	104.5
4	102.5
8	98.5
16	94.0

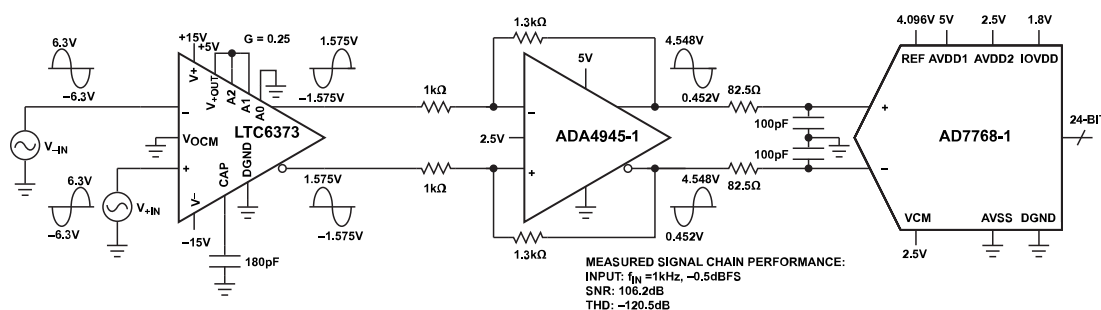
Graph showing Total Harmonic Distortion (THD) in dB versus LTC6373 Gain Setting (G) for an input frequency $f_{IN} = 1\text{ kHz}$. The THD increases as the gain setting increases.

LTC6373 GAIN SETTING (G)	THD (dB)
0.25	-120.5
0.5	-121.0
1	-121.0
2	-120.5
4	-119.5
8	-117.5
16	-113.5

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TYPICAL APPLICATION

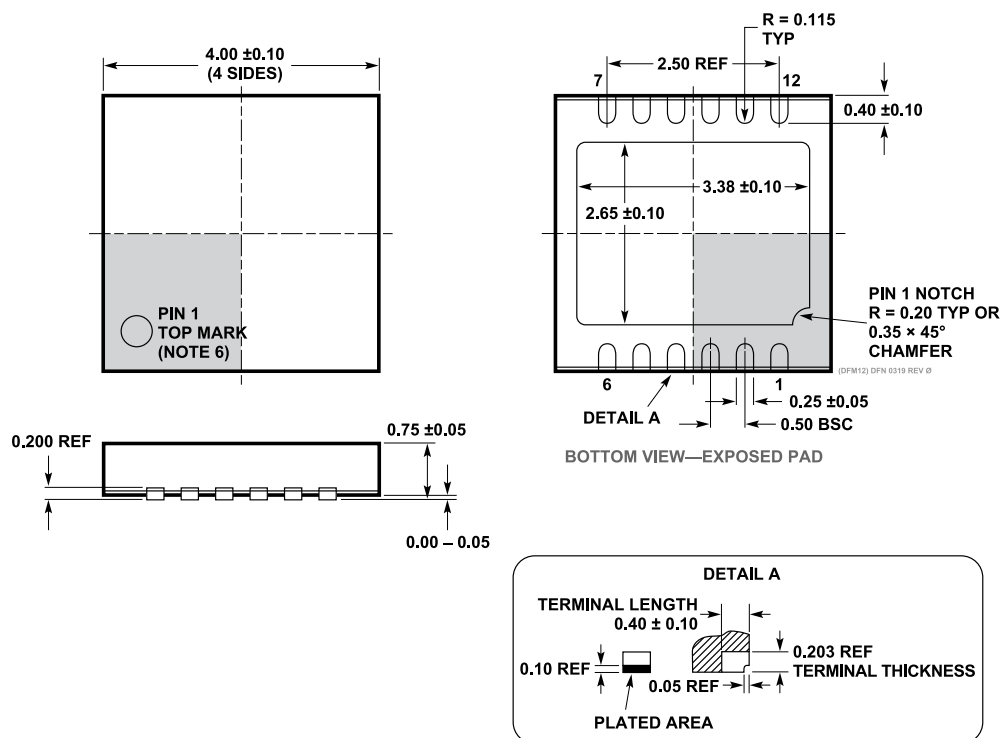
Figure 105. LTC6373 Driving the AD7768-1 Σ - Δ ADC Through a Fully Differential ADC Driver (ADA4945-1)

Related Parts

Table 12.

Part Number	Description	Comments
Programmable-Gain Instrumentation Amplifiers (PGIAs)		
AD8250	G = 1, 2, 5, 10	$V_S = 30\text{V}$, $I_S = 4.1\text{mA}$, $V_{OS} = 200\mu\text{V}$, BW = 10 MHz
AD8251	G = 1, 2, 4, 8	$V_S = 30\text{V}$, $I_S = 4.1\text{mA}$, $V_{OS} = 200\mu\text{V}$, BW = 10 MHz
AD8253	G = 1, 10, 100, 1000	$V_S = 30\text{V}$, $I_S = 4.6\text{mA}$, $V_{OS} = 150\mu\text{V}$, BW = 10 MHz
AD8231	Zero-Drift, G = 1, 2, 4, 8, 16, 32, 64, 128 + Shutdown	$V_S = 5\text{V}$, $I_S = 4\text{mA}$, $V_{OS} = 15\mu\text{V}$, BW = 2.7 MHz
Instrumentation Amplifiers (Resistor-Programmable)		
AD8421	3 nV/ $\sqrt{\text{Hz}}$ Instrumentation Amplifier	$V_S = 36\text{V}$, $I_S = 2\text{mA}$, $V_{OS} = 25\mu\text{V}$, BW = 10 MHz
AD8422	Low Power Instrumentation Amplifier	$V_S = 36\text{V}$, $I_S = 300\mu\text{A}$, $V_{OS} = 25\mu\text{V}$, BW = 2.2 MHz
LT1167	Precision Instrumentation Amplifier	$V_S = 36\text{V}$, $I_S = 900\mu\text{A}$, $V_{OS} = 40\mu\text{V}$, BW = 1 MHz
AD8221	Precision Instrumentation Amplifier	$V_S = 36\text{V}$, $I_S = 900\mu\text{A}$, $V_{OS} = 25\mu\text{V}$, BW = 825 kHz
Fully Differential Amplifiers		
ADA4945-1	High Speed, Fully Differential ADC Driver	3 V-10 V Supply Range, 4 mA/1.4 mA Supply Current in Full and Low Power Modes, -133dBc Distortion at 1 kHz
Analog to Digital Converters (ADCs)		
AD4020	20-Bit, 1.8 Msps, High Precision SAR ADC	1.8 V Supply, Differential Input, 100.5 dB SNR, $\pm 5\text{V}$ Input Range
LTC2378-20	20-Bit, 1 Msps, High Precision SAR ADC	2.5 V Supply, Differential Input, 104 dB SNR, $\pm 5\text{V}$ Input Range
AD4003	18-Bit, 2 Msps, High Precision SAR ADC	1.8 V Supply, Differential Input, 100.5 dB SNR, $\pm 5\text{V}$ Input Range
LTC2379-18	18-Bit, 1.6 Msps, High Precision SAR ADC	2.5 V Supply, Differential Input, 101.2 dB SNR, $\pm 5\text{V}$ Input Range
AD7768/ AD7768-4/ AD7768-1	8-/4-/1-Channel, 24-Bit, Simultaneous-Sampling, 256 ksp/s Σ - Δ ADC	5 V Supply, Differential or Unipolar/Bipolar Input, 108 dB DR, 110.8 kHz BW
AD7134	4-Channel, 24-Bit, Continuous Time, 1.5 Msps Σ - Δ ADC	Easy to Drive Resistive ADC input, 108 dB DR, 392 kHz BW
AD4003	18-Bit, 2 Msps, Data Acquisition μ Module	Integrates ADC Driver, Reference Buffer, and SAR ADC in a $7 \times 7\text{mm}$ BGA Package

OUTLINE DIMENSIONS



NOTE:

1. PACKAGE OUTLINE DOES NOT CONFORM TO JEDEC MO-229
2. DRAWING NOT TO SCALE
3. ALL DIMENSIONS ARE IN MILLIMETERS

4. DIMENSIONS OF EXPOSED PAD ON BOTTOM OF PACKAGE DO NOT INCLUDE MOLD FLASH. MOLD FLASH, IF PRESENT, SHALL NOT EXCEED 0.15mm ON ANY SIDE
5. EXPOSED PAD SHALL BE SOLDER PLATED
6. SHADED AREA IS ONLY A REFERENCE FOR PIN 1 LOCATION ON THE TOP AND BOTTOM OF PACKAGE

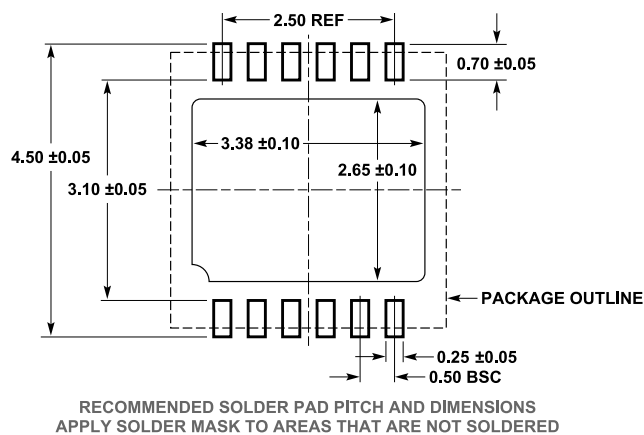


Figure 106. 12-Lead 4 mm x 4 mm DFN
(05-08-1791)

Dimensions shown in millimeters

OUTLINE DIMENSIONS

Updated: February 27, 2023

ORDERING GUIDE

Model ¹	Temperature Range	Package Description	Packing Quantity	Package Option
LTC6373SDFM#PBF	-40°C to +105°C	12-Lead Plastic Side Solderable DFN (4mm × 4mm)		05-08-1791
LTC6373SDFM#TRPBF	-40°C to +105°C	12-Lead Plastic Side Solderable DFN (4mm × 4mm)	Reel, 2500	05-08-1791
LTC6373IDFM#PBF	-40°C to +85°C	12-Lead Plastic Side Solderable DFN (4mm × 4mm)		05-08-1791
LTC6373IDFM#TRPBF	-40°C to +85°C	12-Lead Plastic Side Solderable DFN (4mm × 4mm)	Reel, 2500	05-08-1791

¹ All models are RoHS compliant.

EVALUATION BOARDS

Model ¹	Description
DC2398A	Evaluation Board

¹ DC2398A is RoHS compliant.

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Authorized Distributor

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[DC2398A](#) [LTC6373HDFM#TRPBF](#) [LTC6373IDFM#PBF](#) [LTC6373IDFM#TRPBF](#) [LTC6373SDFM#TRPBF](#)
[LTC6373SDFM#PBF](#)