

## FEATURES

- Measures Up to 12 Battery Cells in Series
- Stackable Architecture Supports 100s of Cells
- Built-In isoSPI™ Interface:
  - 1Mbps Isolated Serial Communications
  - Uses a Single Twisted Pair, Up to 100 Meters
  - Low EMI Susceptibility and Emissions
- 1.2mV Maximum Total Measurement Error
- 290μs to Measure All Cells in a System
- Synchronized Voltage and Current Measurement
- 16-Bit Delta-Sigma ADC with Frequency Programmable 3rd Order Noise Filter
- Engineered for ISO26262 Compliant Systems
- Passive Cell Balancing with Programmable Timer
- 5 General Purpose Digital I/O or Analog Inputs:
  - Temperature or other Sensor Inputs
  - Configurable as an I<sup>2</sup>C or SPI Master
- 4μA Sleep Mode Supply Current
- 48-Lead SSOP Package

## APPLICATIONS

- Electric and Hybrid Electric Vehicles
- Backup Battery Systems
- Grid Energy Storage
- High Power Portable Equipment

## DESCRIPTION

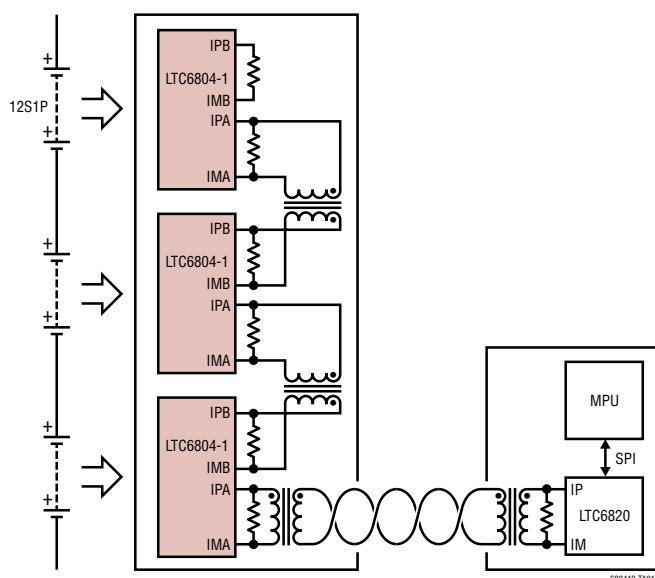
The LTC<sup>®</sup>6804 is a 3rd generation multicell battery stack monitor that measures up to 12 series connected battery cells with a total measurement error of less than 1.2mV. The cell measurement range of 0V to 5V makes the LTC6804 suitable for most battery chemistries. All 12 cell voltages can be captured in 290μs, and lower data acquisition rates can be selected for high noise reduction.

Multiple LTC6804 devices can be connected in series, permitting simultaneous cell monitoring of long, high voltage battery strings. Each LTC6804 has an isoSPI interface for high speed, RF-immune, local area communications. Using the LTC6804-1, multiple devices are connected in a daisy-chain with one host processor connection for all devices. Using the LTC6804-2, multiple devices are connected in parallel to the host processor, with each device individually addressed.

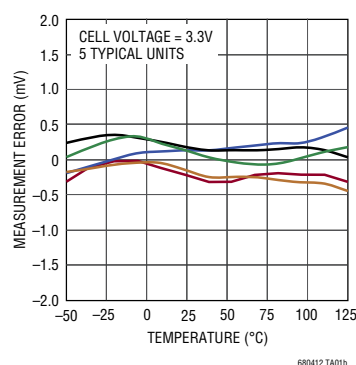
Additional features include passive balancing for each cell, an onboard 5V regulator, and 5 general purpose I/O lines. In sleep mode, current consumption is reduced to 4μA. The LTC6804 can be powered directly from the battery, or from an isolated supply.

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## TYPICAL APPLICATION



**Total Measurement Error  
vs Temperature of 5 Typical Units**



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## ABSOLUTE MAXIMUM RATINGS (Note 1)

Total Supply Voltage $V^+$ to $V^-$ .....	75V	C8 to C4.....	-0.3V to 25V
Input Voltage (Relative to $V^-$ )		C4 to C0.....	-0.3V to 25V
C0.....	-0.3V to 0.3V	Current In/Out of Pins	
C12.....	-0.3V to 75V	All Pins Except $V_{REG}$ , IPA, IMA, IPB, IMB, S(n).. <td>10mA</td>	10mA
C(n).....	-0.3V to MIN (8 • n, 75V)	IPA, IMA, IPB, IMB.....	30mA
S(n).....	-0.3V to MIN (8 • n, 75V)	Operating Temperature Range	
IPA, IMA, IPB, IMB.....	-0.3V to $V_{REG} + 0.3V$	LTC6804I.....	-40°C to 85°C
DRIVE Pin.....	-0.3V to 7V	LTC6804H.....	-40°C to 125°C
All Other Pins.....	-0.3V to 6V	Specified Temperature Range	
Voltage Between Inputs		LTC6804I.....	-40°C to 85°C
$V^+$ to C12.....	-5.5V	LTC6804H.....	-40°C to 125°C
C(n) to C(n - 1).....	-0.3V to 8V	Junction Temperature.....	150°C
S(n) to C(n - 1).....	-0.3V to 8V	Storage Temperature.....	-65°C to 150°C
C12 to C8.....	-0.3V to 25V	Lead Temperature (Soldering, 10sec).....	300°C

## PIN CONFIGURATION

<p>LTC6804-1</p> <p>TOP VIEW</p> <p>G PACKAGE 48-LEAD PLASTIC SSOP</p> <p><math>T_{JMAX} = 150^{\circ}C</math>, <math>\theta_{JA} = 55^{\circ}C/W</math></p> <p>*THE FUNCTION OF THESE PINS DEPENDS ON THE CONNECTION OF ISOMD ISOMD TIED TO <math>V^-</math>: CSB, SCK, SDI, SDO ISOMD TIED TO <math>V_{REG}</math>: IMA, IPA, NC, NC **THIS PIN MUST BE CONNECTED TO <math>V^-</math></p>	<p>LTC6804-2</p> <p>TOP VIEW</p> <p>G PACKAGE 48-LEAD PLASTIC SSOP</p> <p><math>T_{JMAX} = 150^{\circ}C</math>, <math>\theta_{JA} = 55^{\circ}C/W</math></p> <p>*THE FUNCTION OF THESE PINS DEPENDS ON THE CONNECTION OF ISOMD ISOMD TIED TO <math>V^-</math>: CSB, SCK, SDI, SDO ISOMD TIED TO <math>V_{REG}</math>: IMA, IPA, ICMP, IBIAS **THIS PIN MUST BE CONNECTED TO <math>V^-</math></p>
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# LTC6804-1/LTC6804-2

## ORDER INFORMATION

<http://www.linear.com/product/LTC6804-1#orderinfo>

TUBE	TAPE AND REEL	PART MARKING*	PACKAGE DESCRIPTION	SPECIFIED TEMPERATURE RANGE
LTC6804IG-1#PBF	LTC6804IG-1#TRPBF	LTC6804G-1	48-Lead Plastic SSOP	-40°C to 85°C
LTC6804HG-1#PBF	LTC6804HG-1#TRPBF	LTC6804G-1	48-Lead Plastic SSOP	-40°C to 125°C
LTC6804IG-2#PBF	LTC6804IG-2#TRPBF	LTC6804G-2	48-Lead Plastic SSOP	-40°C to 85°C
LTC6804HG-2#PBF	LTC6804HG-2#TRPBF	LTC6804G-2	48-Lead Plastic SSOP	-40°C to 125°C

Consult LTC Marketing for parts specified with wider operating temperature ranges. \*The temperature grade is identified by a label on the shipping container. Parts ending with PBF are RoHS and WEEE compliant.

For more information on lead free part marking, go to: <http://www.linear.com/leadfree/>

For more information on tape and reel specifications, go to: <http://www.linear.com/tapeandreel/>. Some packages are available in 500 unit reels through designated sales channels with #TRMPBF suffix.

## ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . The test conditions are  $V^+ = 3.9.6\text{V}$ ,  $V_{\text{REG}} = 5.0\text{V}$  unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
ADC DC Specifications						
	Measurement Resolution		●	0.1		mV/bit
	ADC Offset Voltage	(Note 2)	●	0.1		mV
	ADC Gain Error	(Note 2)	●	0.01 0.02		% %
Total Measurement Error (TME) in Normal Mode	C(n) to C(n-1), GPIO(n) to $V^- = 0$			±0.2		mV
	C(n) to C(n-1) = 2.0			±0.1	±0.8	mV
	C(n) to C(n-1), GPIO(n) to $V^- = 2.0$	●			±1.4	mV
	C(n) to C(n-1) = 3.3			±0.2	±1.2	mV
	C(n) to C(n-1), GPIO(n) to $V^- = 3.3$	●			±2.2	mV
	C(n) to C(n-1) = 4.2			±0.3	±1.6	mV
	C(n) to C(n-1), GPIO(n) to $V^- = 4.2$	●			±2.8	mV
	C(n) to C(n-1), GPIO(n) to $V^- = 5.0$			±1		mV
	Sum of Cells, $V(\text{CO}) = V^-$	●		±0.2	±0.75	%
	Internal Temperature, T = Maximum Specified Temperature			±5		°C
	$V_{\text{REG}}$ Pin	●		±0.1	±0.25	%
	$V_{\text{REF2}}$ Pin	●		±0.02	±0.1	%
	Digital Supply Voltage $V_{\text{REGD}}$	●		±0.1	±1	%

**ELECTRICAL CHARACTERISTICS** The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . The test conditions are  $V^+ = 39.6\text{V}$ ,  $V_{\text{REG}} = 5.0\text{V}$  unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS	
	Total Measurement Error (TME) in Filtered Mode	C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 0		±0.1			mV	
		C(n) to C(n – 1) = 2.0		±0.1	±0.8		mV	
		C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 2.0	●			±1.4		mV
		C(n) to C(n – 1) = 3.3		±0.2	±1.2		mV	
		C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 3.3	●			±2.2		mV
		C(n) to C(n – 1) = 4.2		±0.3	±1.6		mV	
		C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 4.2	●			±2.8		mV
		C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 5.0		±1			mV	
		Sum of Cells, V(CO) = V <sup>-</sup>	●	±0.2	±0.75		%	
		Internal Temperature, T = Maximum Specified Temperature		±5			°C	
		V <sub>REG</sub> Pin	●	±0.1	±0.25		%	
		V <sub>REF2</sub> Pin	●	±0.02	±0.1		%	
		Digital Supply Voltage V <sub>REGD</sub>	●	±0.1	±1		%	
			Total Measurement Error (TME) in Fast Mode	C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 0		±2		
C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 2.0	●					±4		mV
C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 3.3	●					±4.7		mV
C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 4.2	●					±8.3		mV
C(n) to C(n – 1), GPIO(n) to V <sup>-</sup> = 5.0				±10			mV	
Sum of Cells, V(CO) = V <sup>-</sup>	●			±0.3	±1		%	
Internal Temperature, T = Maximum Specified Temperature				±5			°C	
V <sub>REG</sub> Pin	●			±0.3	±1		%	
V <sub>REF2</sub> Pin	●			±0.1	±0.25		%	
Digital Supply Voltage V <sub>REGD</sub>	●			±0.2	±2		%	
	Input Range			C(n), n = 1 to 12	●	C(n – 1)	C(n – 1) + 5	
		C0	●	0				
		GPIO(n), n = 1 to 5	●	0	5		V	
I <sub>L</sub>	Input Leakage Current When Inputs Are Not Being Measured	C(n), n = 0 to 12	●	10	±250		nA	
		GPIO(n), n = 1 to 5	●	10	±250		nA	
	Input Current When Inputs Are Being Measured	C(n), n = 0 to 12		±2			μA	
		GPIO(n), n = 1 to 5		±2			μA	
	Input Current During Open Wire Detection		●	70	100	130	μA	

# LTC6804-1/LTC6804-2

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SYMBOL	PARAMETER	CONDITIONS				MIN	TYP	MAX	UNITS
Voltage Reference Specifications									
V <sub>REF1</sub>	1st Reference Voltage	V <sub>REF1</sub> Pin, No Load			●	3.1	3.2	3.3	V
	1st Reference Voltage TC	V <sub>REF1</sub> Pin, No Load				3			ppm/°C
	1st Reference Voltage Hysteresis	V <sub>REF1</sub> Pin, No Load				20			ppm
	1st Reference Long Term Drift	V <sub>REF1</sub> Pin, No Load				20			ppm/√kHr
V <sub>REF2</sub>	2nd Reference Voltage	V <sub>REF2</sub> Pin, No Load			●	2.990	3	3.010	V
		V <sub>REF2</sub> Pin, 5k Load to V <sup>-</sup>			●	2.988	3	3.012	V
	2nd Reference Voltage TC	V <sub>REF2</sub> Pin, No Load				10			ppm/°C
	2nd Reference Voltage Hysteresis	V <sub>REF2</sub> Pin, No Load				100			ppm
	2nd Reference Long Term Drift	V <sub>REF2</sub> Pin, No Load				60			ppm/√kHr
	General DC Specifications								
I <sub>VP</sub>	V <sup>+</sup> Supply Current (See Figure 1: LTC6804 Operation State Diagram)	State: Core = SLEEP, isoSPI = IDLE	V <sub>REG</sub> = 0V		3.8			6	μA
			V <sub>REG</sub> = 0V	●	3.8			10	μA
			V <sub>REG</sub> = 5V		1.6			3	μA
			V <sub>REG</sub> = 5V	●	1.6			5	μA
		State: Core = STANDBY		18			32	50	μA
			●	10			32	60	μA
		State: Core = REFUP or MEASURE		0.4			0.55	0.7	mA
			●	0.375			0.55	0.725	mA
I <sub>REG(CORE)</sub>	V <sub>REG</sub> Supply Current (See Figure 1: LTC6804 Operation State diagram)	State: Core = SLEEP, isoSPI = IDLE	V <sub>REG</sub> = 5V		2.2			4	μA
			V <sub>REG</sub> = 5V	●	2.2			6	μA
		State: Core = STANDBY		10			35	60	μA
			●	6			35	65	μA
		State: Core = REFUP		0.2			0.45	0.7	mA
			●	0.15			0.45	0.75	mA
		State: Core = MEASURE		10.8			11.5	12.2	mA
			●	10.7			11.5	12.3	mA
I <sub>REG(isoSPI)</sub>	Additional V <sub>REG</sub> Supply Current if isoSPI in READY/ACTIVE States  Note: ACTIVE State Current Assumes t <sub>CLK</sub> = 1μs, (Note 3)	LTC6804-2: ISOMD = 1, R <sub>B1</sub> + R <sub>B2</sub> = 2k	READY	●	3.9	4.8	5.8	mA	
			ACTIVE	●	5.1	6.1	7.3	mA	
		LTC6804-1: ISOMD = 0, R <sub>B1</sub> + R <sub>B2</sub> = 2k	READY	●	3.7	4.6	5.6	mA	
			ACTIVE	●	5.7	6.8	8.1	mA	
		LTC6804-1: ISOMD = 1, R <sub>B1</sub> + R <sub>B2</sub> = 2k	READY	●	6.5	7.8	9.5	mA	
			ACTIVE	●	10.2	11.3	13.3	mA	
		LTC6804-2: ISOMD = 1, R <sub>B1</sub> + R <sub>B2</sub> = 20k	READY	●	1.3	2.1	3	mA	
			ACTIVE	●	1.6	2.5	3.5	mA	
		LTC6804-1: ISOMD = 0, R <sub>B1</sub> + R <sub>B2</sub> = 20k	READY	●	1.1	1.9	2.8	mA	
			ACTIVE	●	1.5	2.3	3.3	mA	
		LTC6804-1: ISOMD = 1, R <sub>B1</sub> + R <sub>B2</sub> = 20k	READY	●	2.1	3.3	4.9	mA	
			ACTIVE	●	2.7	4.1	5.8	mA	

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SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
	$V^+$ Supply Voltage	TME Specifications Met (Note 6)	●	11	40	55	V
$V_{\text{REG}}$	$V_{\text{REG}}$ Supply Voltage	TME Supply Rejection $< 1\text{mV/V}$	●	4.5	5	5.5	V
	DRIVE output voltage	Sourcing $1\mu\text{A}$		5.4	5.6	5.8	V
			●	5.2	5.6	6.0	V
		Sourcing $500\mu\text{A}$	●	5.1	5.6	6.1	V
$V_{\text{REGD}}$	Digital Supply Voltage		●	2.7	3.0	3.6	V
	Discharge Switch ON Resistance	$V_{\text{CELL}} = 3.6\text{V}$	●		10	25	$\Omega$
	Thermal Shutdown Temperature				150		$^\circ\text{C}$
$V_{\text{OL(WDT)}}$	Watchdog Timer Pin Low	WDT Pin Sinking $4\text{mA}$	●			0.4	V
$V_{\text{OL(GPIO)}}$	General Purpose I/O Pin Low	GPIO Pin Sinking $4\text{mA}$ (Used as Digital Output)	●			0.4	V

#### ADC Timing Specifications

$t_{\text{CYCLE}}$ (Figure 3)	Measurement + Calibration Cycle Time When Starting from the REFUP State in Normal Mode	Measure 12 Cells	●	2120	2335	2480	$\mu\text{s}$
		Measure 2 Cells	●	365	405	430	$\mu\text{s}$
		Measure 12 Cells and 2 GPIO Inputs	●	2845	3133	3325	$\mu\text{s}$
	Measurement + Calibration Cycle Time When Starting from the REFUP State in Filtered Mode	Measure 12 Cells	●	183	201.3	213.5	ms
		Measure 2 Cells	●	30.54	33.6	35.64	ms
		Measure 12 Cells and 2 GPIO Inputs	●	244	268.4	284.7	ms
	Measurement + Calibration Cycle Time When Starting from the REFUP State in Fast Mode	Measure 12 Cells	●	1010	1113	1185	$\mu\text{s}$
		Measure 2 Cells	●	180	201	215	$\mu\text{s}$
		Measure 12 Cells and 2 GPIO Inputs	●	1420	1564	1660	$\mu\text{s}$
$t_{\text{SKEW1}}$ (Figure 6)	Skew Time. The Time Difference between C12 and GPIO2 Measurements, Command = ADCVAX	Fast Mode	●	189	208	221	$\mu\text{s}$
		Normal Mode	●	493	543	576	$\mu\text{s}$
$t_{\text{SKEW2}}$ (Figure 3)	Skew Time. The Time Difference between C12 and C0 Measurements, Command = ADCV	Fast Mode	●	211	233	248	$\mu\text{s}$
		Normal Mode	●	609	670	711	$\mu\text{s}$
$t_{\text{WAKE}}$	Regulator Start-Up Time	$V_{\text{REG}}$ Generated from Drive Pin (Figure 28)	●		100	300	$\mu\text{s}$
$t_{\text{SLEEP}}$	Watchdog or Software Discharge Timer	SWTEN Pin = 0 or DCTO[3:0] = 0000	●	1.8	2	2.2	sec
		SWTEN Pin = 1 and DCTO[3:0] $\neq$ 0000		0.5		120	min
$t_{\text{REFUP}}$ (Figure 1, Figures 3 to 7)	Reference Wake-Up Time	State: Core = STANDBY	●	2.7	3.5	4.4	ms
		State: Core = REFUP	●			0	ms
$f_s$	ADC Clock Frequency		●	3.0	3.3	3.5	MHz

#### SPI Interface DC Specifications

$V_{\text{IH(SPI)}}$	SPI Pin Digital Input Voltage High	Pins CSB, SCK, SDI	●	2.3			V
$V_{\text{IL(SPI)}}$	SPI Pin Digital Input Voltage Low	Pins CSB, SCK, SDI	●			0.8	V
$V_{\text{IH(CFG)}}$	Configuration Pin Digital Input Voltage High	Pins ISOMD, SWTEN, GPIO1 to GPIO5, A0 to A3	●	2.7			V
$V_{\text{IL(CFG)}}$	Configuration Pin Digital Input Voltage Low	Pins ISOMD, SWTEN, GPIO1 to GPIO5, A0 to A3	●			1.2	V

# LTC6804-1/LTC6804-2

**ELECTRICAL CHARACTERISTICS** The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . The test conditions are  $V^+ = 39.6\text{V}$ ,  $V_{\text{REG}} = 5.0\text{V}$  unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
$I_{\text{LEAK(DIG)}}$	Digital Input Current	Pins CSB, SCK, SDI, ISOMD, SWTEN, A0 to A3	●		$\pm 1$	$\mu\text{A}$
$V_{\text{OL(SDO)}}$	Digital Output Low	Pin SDO Sinking 1mA	●		0.3	V

## isoSPI DC Specifications (See Figure 16)

$V_{\text{BIAS}}$	Voltage on IBIAS Pin	READY/ACTIVE State IDLE State	●	1.9	2.0 0	2.1	V V
$I_{\text{B}}$	Isolated Interface Bias Current	$R_{\text{BIAS}} = 2\text{k}$ to $20\text{k}$	●	0.1		1.0	mA
$A_{\text{IB}}$	Isolated Interface Current Gain	$V_A \leq 1.6\text{V}$ $I_{\text{B}} = 1\text{mA}$ $I_{\text{B}} = 0.1\text{mA}$	● ●	18 18	20 20	22 24.5	mA/mA mA/mA
$V_A$	Transmitter Pulse Amplitude	$V_A =  V_{\text{IP}} - V_{\text{IM}} $	●			1.6	V
$V_{\text{ICMP}}$	Threshold-Setting Voltage on ICMP Pin	$V_{\text{TCMP}} = A_{\text{TCMP}} \cdot V_{\text{ICMP}}$	●	0.2		1.5	V
$I_{\text{LEAK(ICMP)}}$	Input Leakage Current on ICMP Pin	$V_{\text{ICMP}} = 0\text{V}$ to $V_{\text{REG}}$	●			$\pm 1$	$\mu\text{A}$
$I_{\text{LEAK(IP/IM)}}$	Leakage Current on IP and IM Pins	IDLE State, $V_{\text{IP}}$ or $V_{\text{IM}} = 0\text{V}$ to $V_{\text{REG}}$	●			$\pm 1$	$\mu\text{A}$
$A_{\text{TCMP}}$	Receiver Comparator Threshold Voltage Gain	$V_{\text{CM}} = V_{\text{REG}}/2$ to $V_{\text{REG}} - 0.2\text{V}$ , $V_{\text{ICMP}} = 0.2\text{V}$ to $1.5\text{V}$	●	0.4	0.5	0.6	V/V
$V_{\text{CM}}$	Receiver Common Mode Bias	IP/IM Not Driving		$(V_{\text{REG}} - V_{\text{ICMP}}/3 - 167\text{mV})$			V
$R_{\text{IN}}$	Receiver Input Resistance	Single-Ended to IPA, IMA, IPB, IMB	●	27	35	43	$\text{k}\Omega$

## isoSPI Idle/Wakeup Specifications (See Figure 21)

$V_{\text{WAKE}}$	Differential Wake-Up Voltage	$t_{\text{DWELL}} = 240\text{ns}$	●	200			mV
$t_{\text{DWELL}}$	Dwell Time at $V_{\text{WAKE}}$ Before Wake Detection	$V_{\text{WAKE}} = 200\text{mV}$	●	240			ns
$t_{\text{READY}}$	Startup Time After Wake Detection		●			10	$\mu\text{s}$
$t_{\text{IDLE}}$	Idle Timeout Duration		●	4.3	5.5	6.7	ms

## isoSPI Pulse Timing Specifications (See Figure 19)

$t_{1/2\text{PW(CS)}}$	Chip-Select Half-Pulse Width		●	120	150	180	ns
$t_{\text{INV(CS)}}$	Chip-Select Pulse Inversion Delay		●			200	ns
$t_{1/2\text{PW(D)}}$	Data Half-Pulse Width		●	40	50	60	ns
$t_{\text{INV(D)}}$	Data Pulse Inversion Delay		●			70	ns

## SPI Timing Requirements (See Figure 15 and Figure 20)

$t_{\text{CLK}}$	SCK Period	(Note 4)	●	1			$\mu\text{s}$
$t_1$	SDI Setup Time before SCK Rising Edge		●	25			ns
$t_2$	SDI Hold Time after SCK Rising Edge		●	25			ns
$t_3$	SCK Low	$t_{\text{CLK}} = t_3 + t_4 \geq 1\mu\text{s}$	●	200			ns
$t_4$	SCK High	$t_{\text{CLK}} = t_3 + t_4 \geq 1\mu\text{s}$	●	200			ns
$t_5$	CSB Rising Edge to CSB Falling Edge		●	0.65			$\mu\text{s}$
$t_6$	SCK Rising Edge to CSB Rising Edge	(Note 4)	●	0.8			$\mu\text{s}$
$t_7$	CSB Falling Edge to SCK Rising Edge	(Note 4)	●	1			$\mu\text{s}$



**ELECTRICAL CHARACTERISTICS** The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . The test conditions are  $V^+ = 39.6\text{V}$ ,  $V_{\text{REG}} = 5.0\text{V}$  unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
<b>isoSPI Timing Specifications (See Figure 19)</b>							
$t_8$	SCK Falling Edge to SDO Valid	(Note 5)	●			60	ns
$t_9$	SCK Rising Edge to Short $\pm 1$ Transmit		●			50	ns
$t_{10}$	CSB Transition to Long $\pm 1$ Transmit		●			60	ns
$t_{11}$	CSB Rising Edge to SDO Rising	(Note 5)	●			200	ns
$t_{\text{RTN}}$	Data Return Delay		●		430	525	ns
$t_{\text{DSY(CS)}}$	Chip-Select Daisy-Chain Delay		●		150	200	ns
$t_{\text{DSY(D)}}$	Data Daisy-Chain Delay		●		300	360	ns
$t_{\text{LAG}}$	Data Daisy-Chain Lag (vs Chip-Select)		●	0	35	70	ns
$t_{6(\text{GOV})}$	Data to Chip-Select Pulse Governor		●	0.8		1.05	$\mu\text{s}$

**Note 1:** Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

**Note 2:** The ADC specifications are guaranteed by the Total Measurement Error specification.

**Note 3:** The ACTIVE state current is calculated from DC measurements. The ACTIVE state current is the additional average supply current into  $V_{\text{REG}}$  when there is continuous 1MHz communications on the isoSPI ports with 50% data 1's and 50% data 0's. Slower clock rates reduce the supply current. See Applications Information section for additional details.

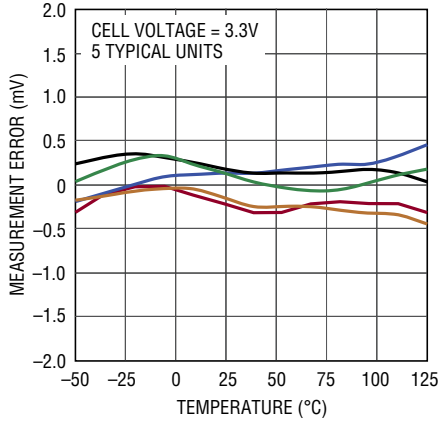
**Note 4:** These timing specifications are dependent on the delay through the cable, and include allowances for 50ns of delay each direction. 50ns corresponds to 10m of CAT-5 cable (which has a velocity of propagation of 66% the speed of light). Use of longer cables would require derating these specs by the amount of additional delay.

**Note 5:** These specifications do not include rise or fall time of SDO. While fall time (typically 5ns due to the internal pull-down transistor) is not a concern, rising-edge transition time  $t_{\text{RISE}}$  is dependent on the pull-up resistance and load capacitance on the SDO pin. The time constant must be chosen such that SDO meets the setup time requirements of the MCU.

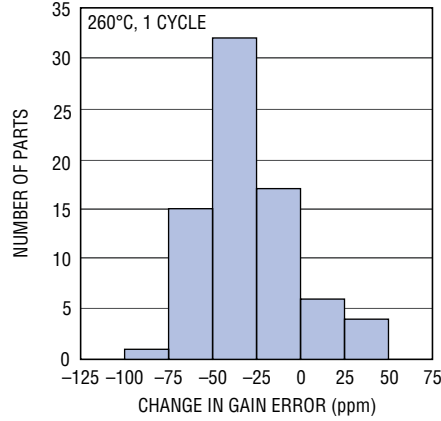
**Note 6:**  $V^+$  needs to be greater than or equal to the highest C(n) voltage for accurate measurements. See the graph Top Cell Measurement Error vs  $V^+$ .

## TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

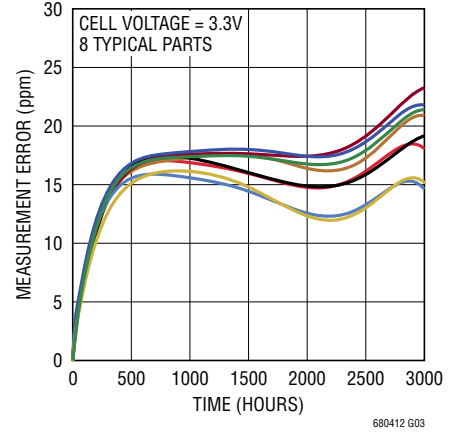
**Measurement Error vs Temperature**



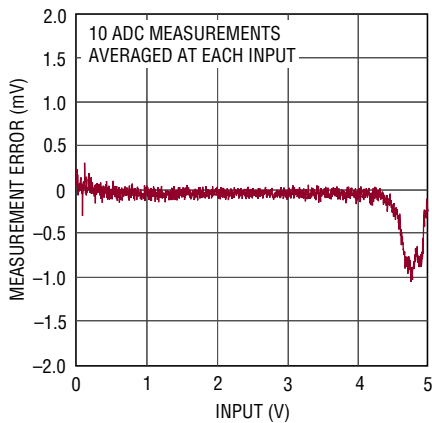
**Measurement Error Due to IR Reflow**



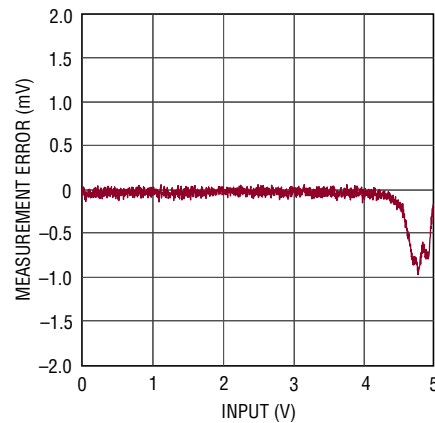
**Measurement Error Long-Term Drift**



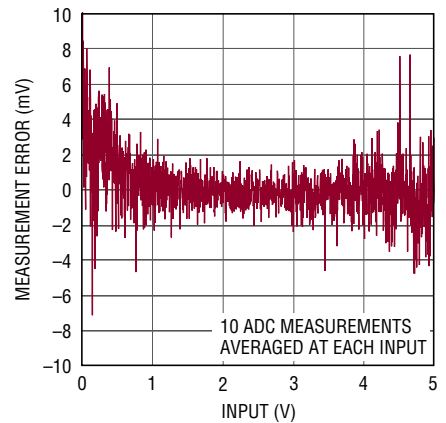
**Measurement Error vs Input, Normal Mode**



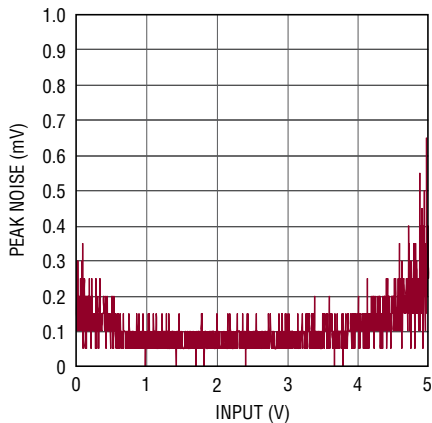
**Measurement Error vs Input, Filtered Mode**



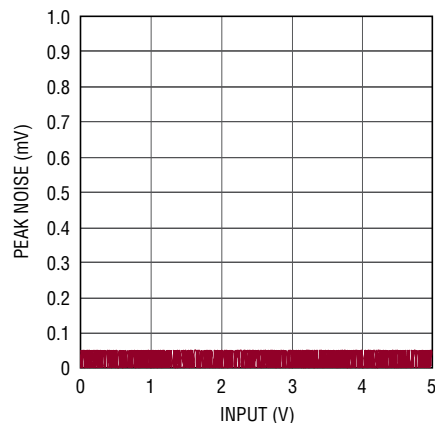
**Measurement Error vs Input, Fast Mode**



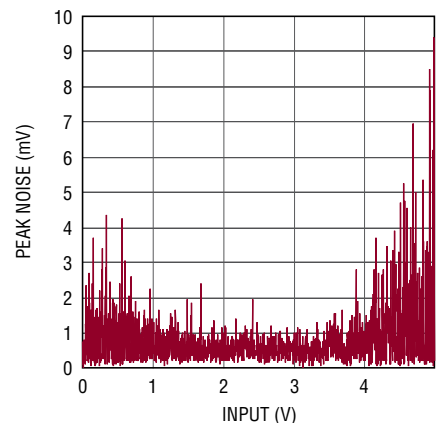
**Measurement Noise vs Input, Normal Mode**



**Measurement Noise vs Input, Filtered Mode**

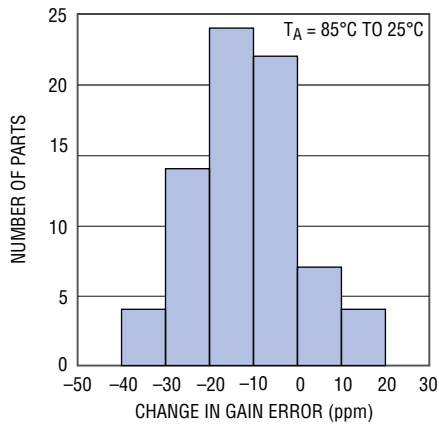


**Measurement Noise vs Input, Fast Mode**

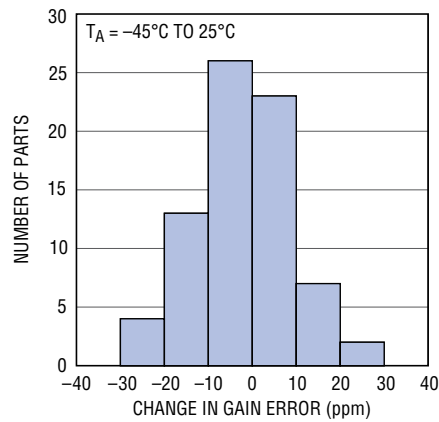


# TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

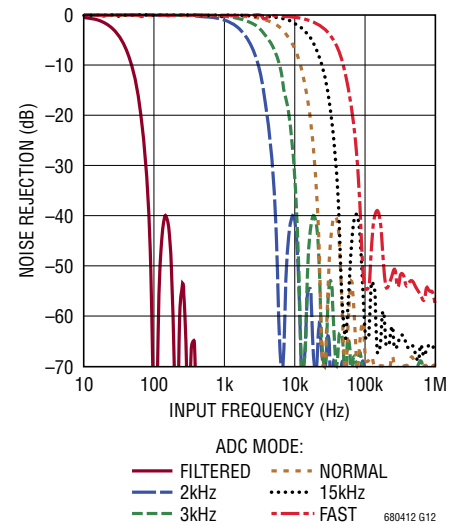
**Measurement Gain Error Hysteresis, Hot**



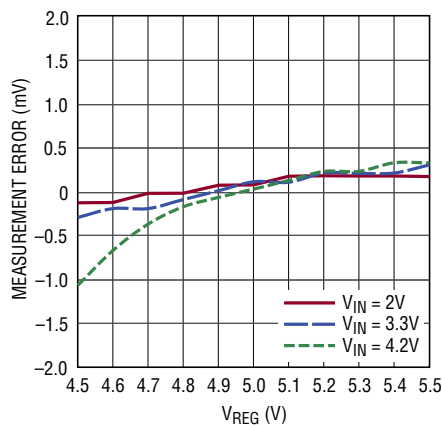
**Measurement Gain Error Hysteresis, Cold**



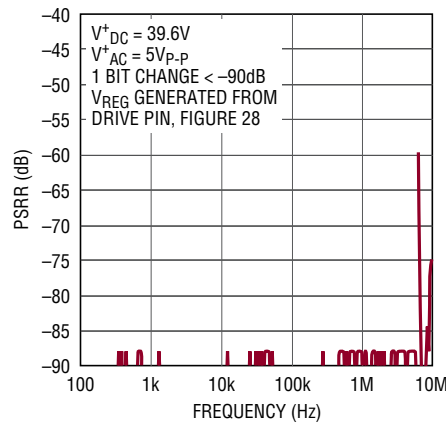
**Noise Filter Response**



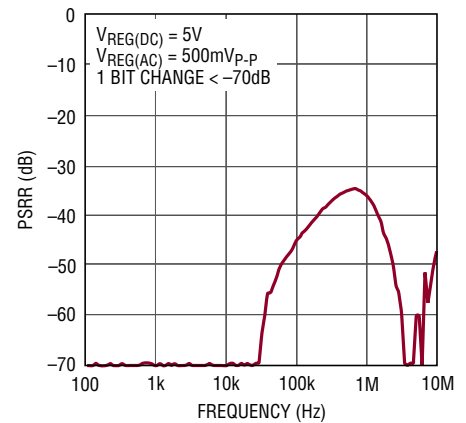
**Measurement Error vs  $V_{\text{REG}}$**



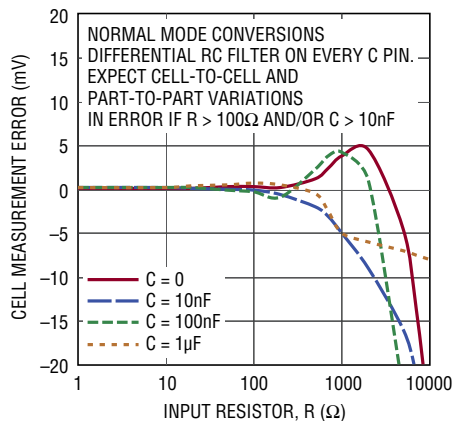
**Measurement Error  $V^+$  PSRR vs Frequency**



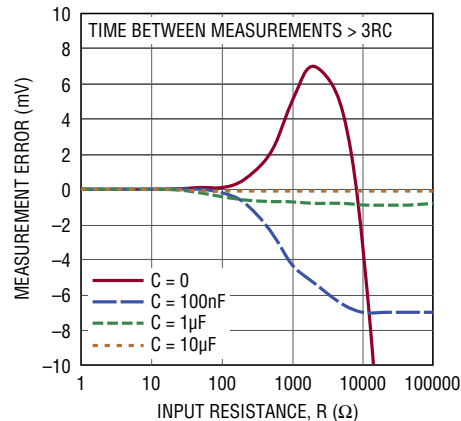
**Measurement Error  $V_{\text{REG}}$  PSRR vs Frequency**



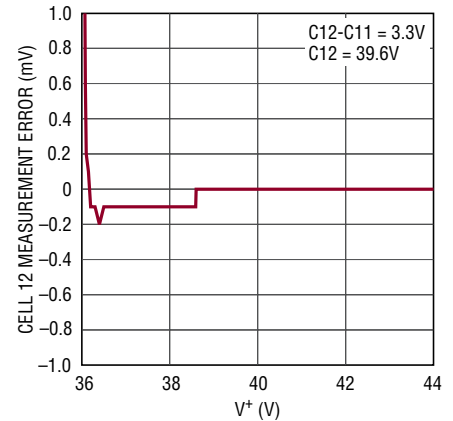
**Cell Measurement Error vs Input RC Values**



**GPIO Measurement Error vs Input RC Values**

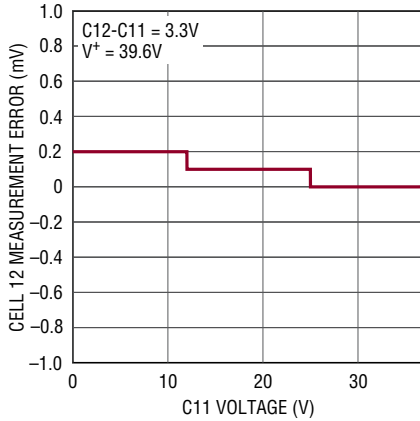


**Top Cell Measurement Error vs  $V^+$**



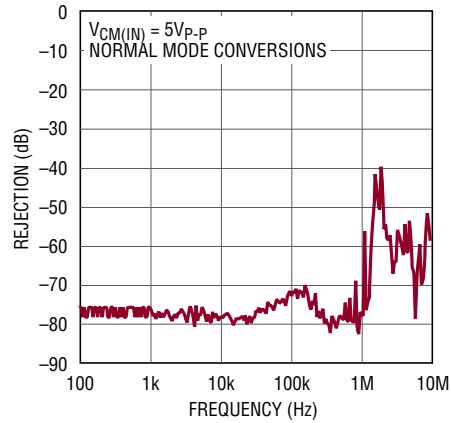
# TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

### Cell Measurement Error vs Common Mode Voltage



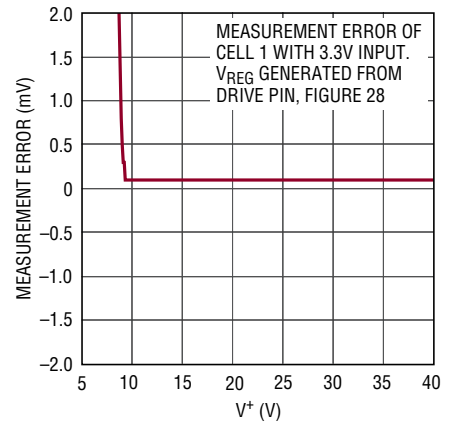
680412 G19

### Cell Measurement CMRR vs Frequency



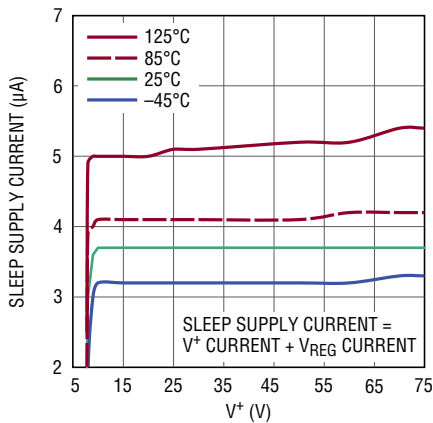
680412 G20

### Measurement Error vs V+



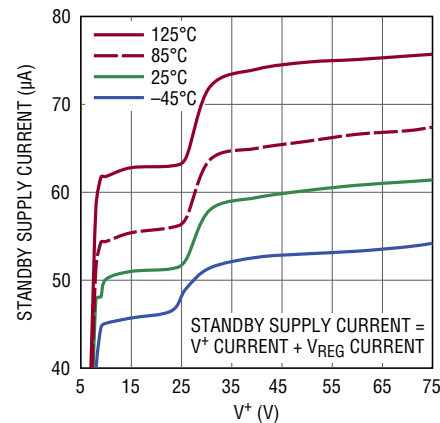
680412 G21

### Sleep Supply Current vs V+



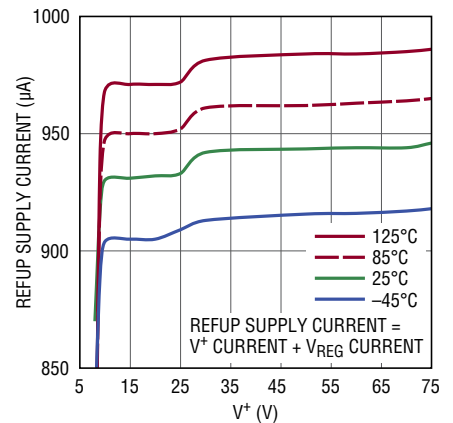
680412 G22

### Standby Supply Current vs V+



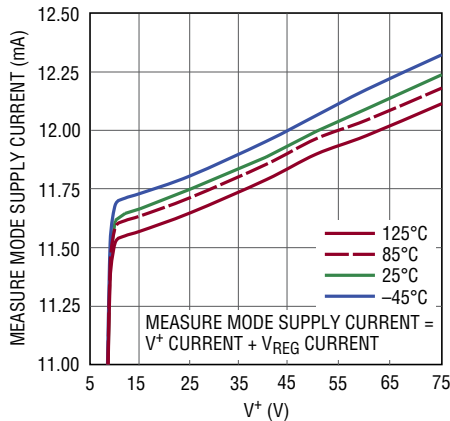
680412 G23

### REFUP Supply Current vs V+



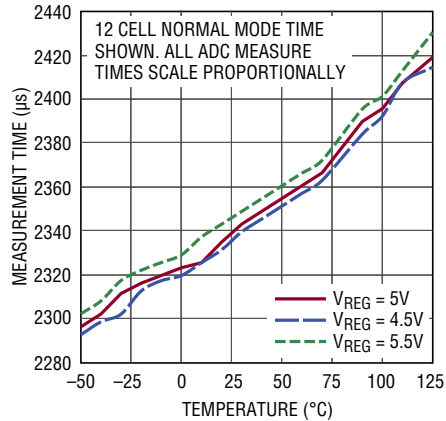
680412 G24

### Measure Mode Supply Current vs V+



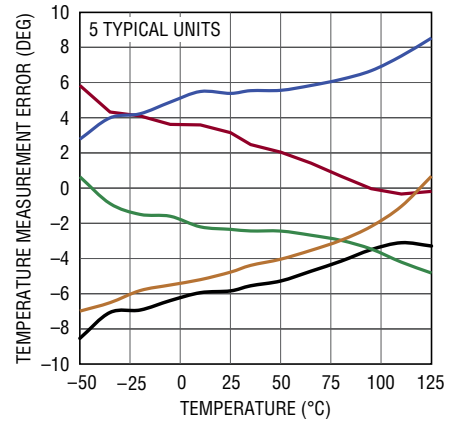
680412 G25

### Measurement Time vs Temperature



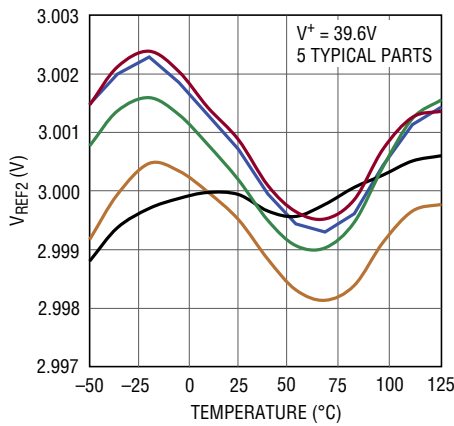
680412 G26

### Internal Die Temperature Measurement Error vs Temperature

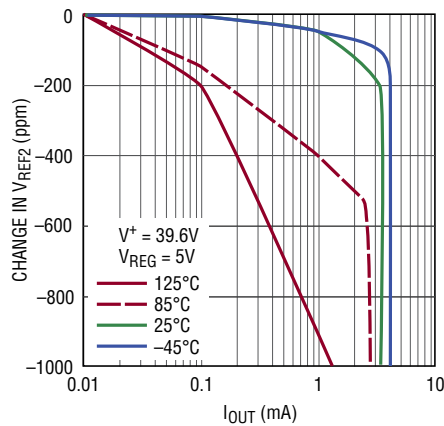


680412 G27

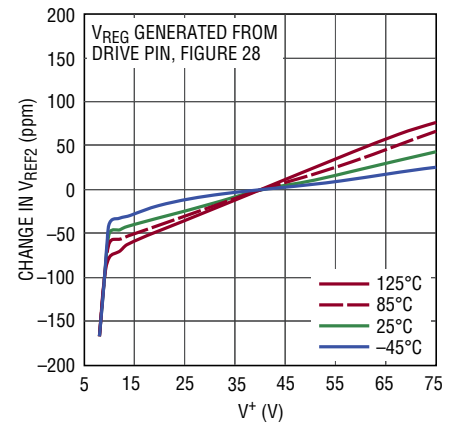
# TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

**V<sub>REF2</sub> vs Temperature**

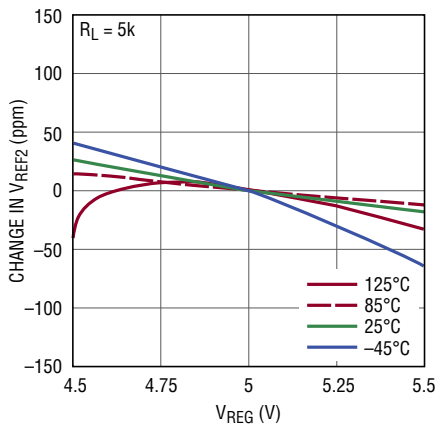
680412 G28

**V<sub>REF2</sub> Load Regulation**

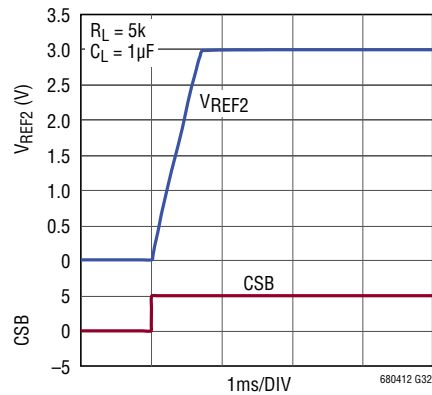
680412 G29

**V<sub>REF2</sub> V<sup>+</sup> Line Regulation**

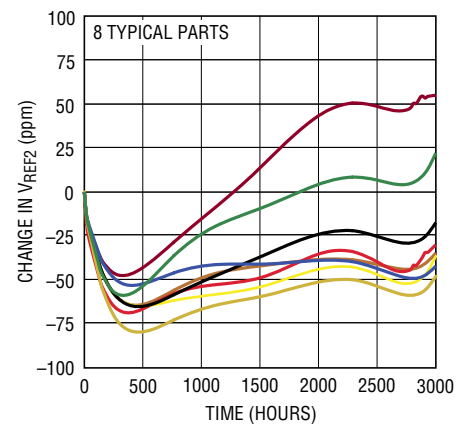
580412 G30

**V<sub>REF2</sub> V<sub>REG</sub> Line Regulation**

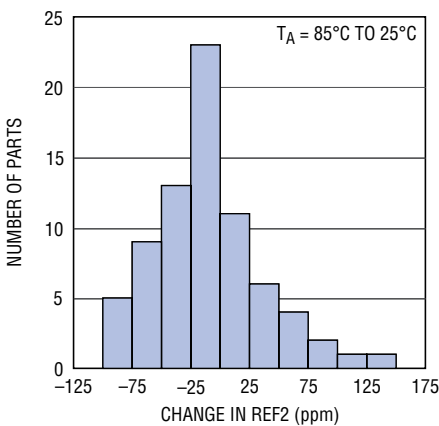
680412 G31

**V<sub>REF2</sub> Power-Up**

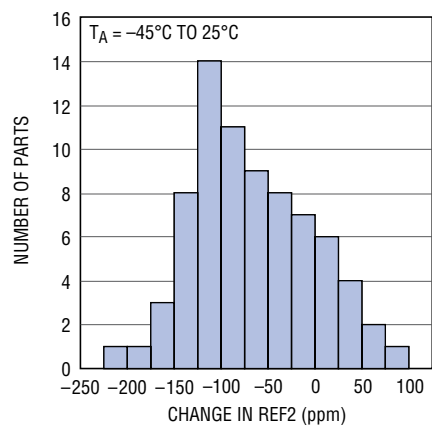
680412 G32

**V<sub>REF2</sub> Long-Term Drift**

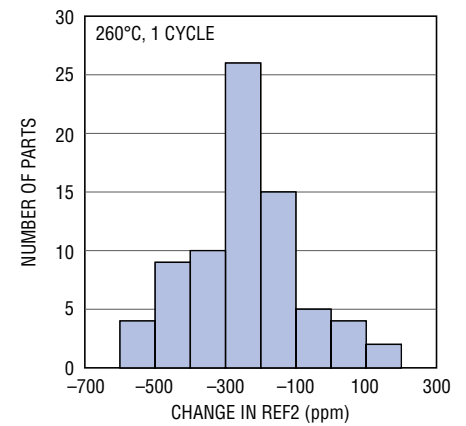
680412 G33

**V<sub>REF2</sub> Hysteresis, Hot**

680412 G34

**V<sub>REF2</sub> Hysteresis, Cold**

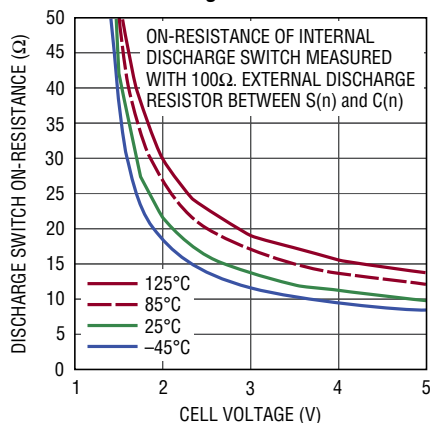
680412 G35

**V<sub>REF2</sub> Change Due to IR Reflow**

680412 G36

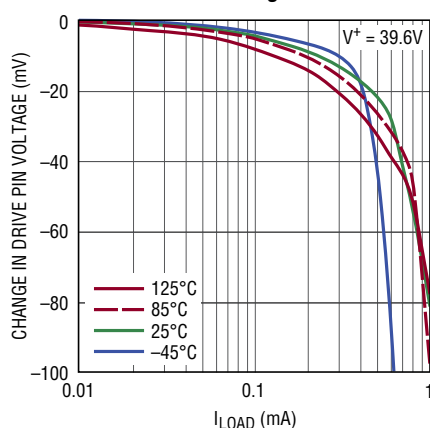
# TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

## Discharge Switch On-Resistance vs Cell Voltage



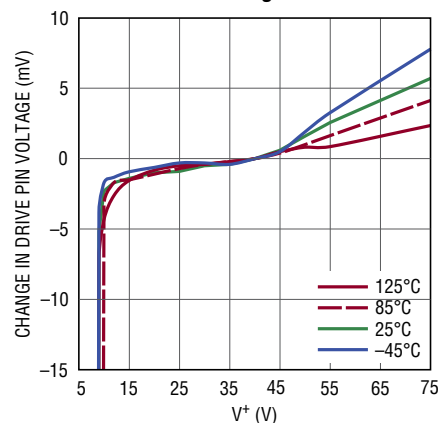
680412 G37

## Drive Pin Load Regulation



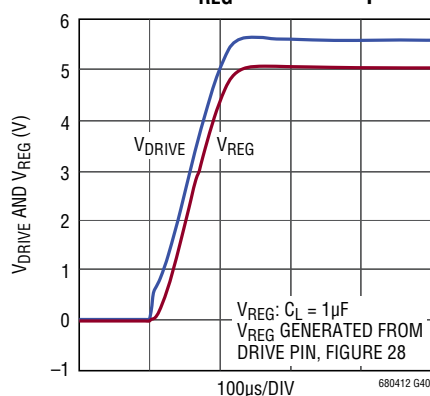
680412 G38

## Drive Pin Line Regulation



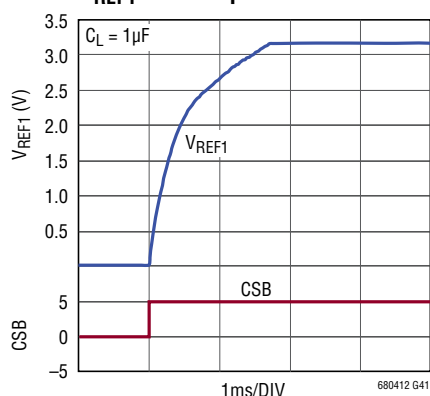
680412 G39

## Drive and VREG Pin Power-Up



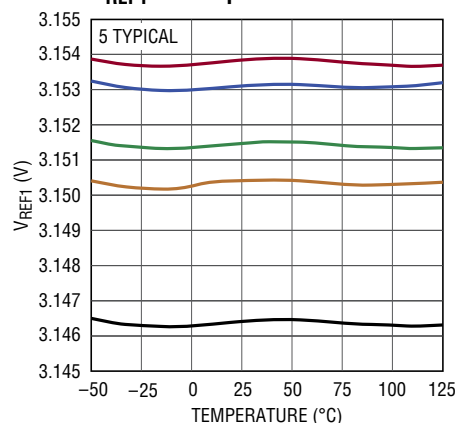
680412 G40

## VREF1 Power-Up



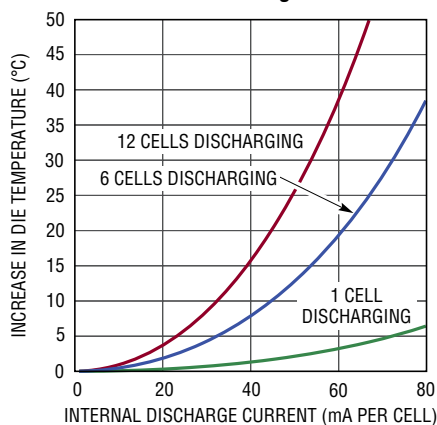
680412 G41

## VREF1 vs Temperature



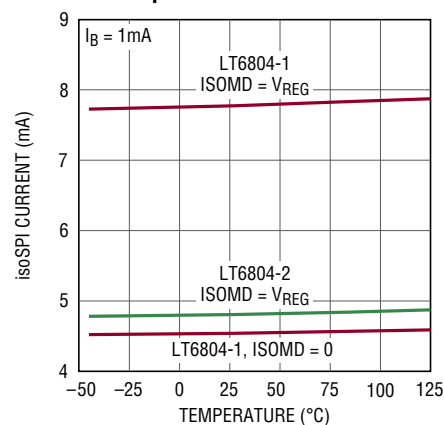
680412 G42

## Internal Die Temperature Increase vs Discharge Current



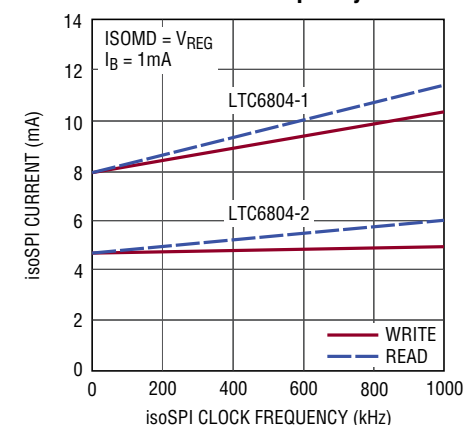
680412 G43

## isoSPI Current (READY) vs Temperature



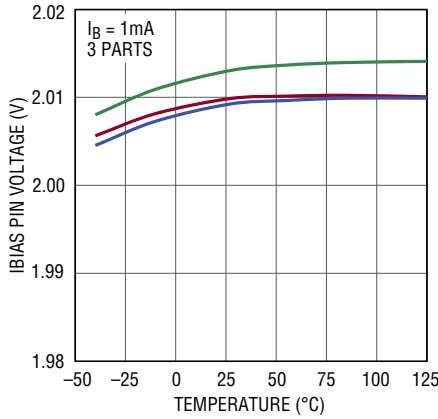
680412 G44

## isoSPI Current (READY/ACTIVE) vs isoSPI Clock Frequency

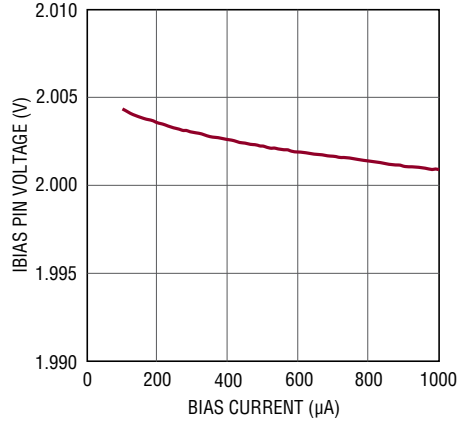


680412 G45

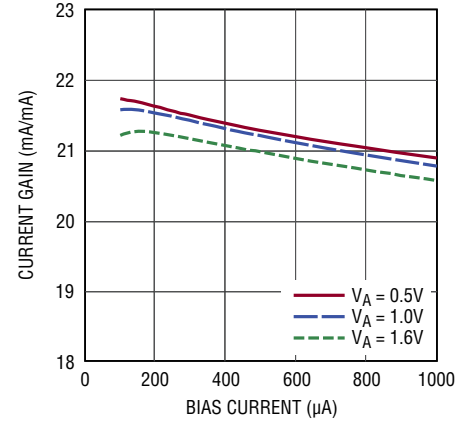
# TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

**IBIAS Voltage vs Temperature**


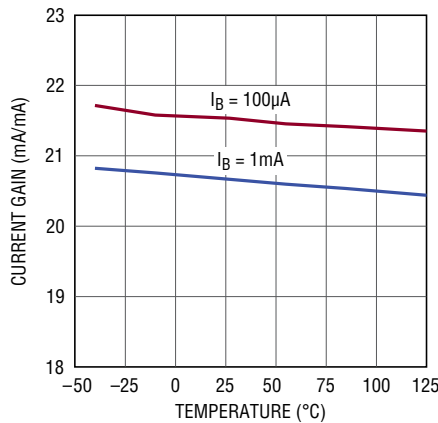
680412 G46

**IBIAS Voltage Load Regulation**


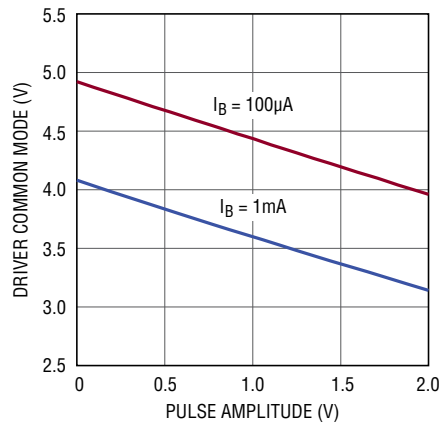
408912 G47

**isoSPI Driver Current Gain (Port A/Port B) vs Bias Current**


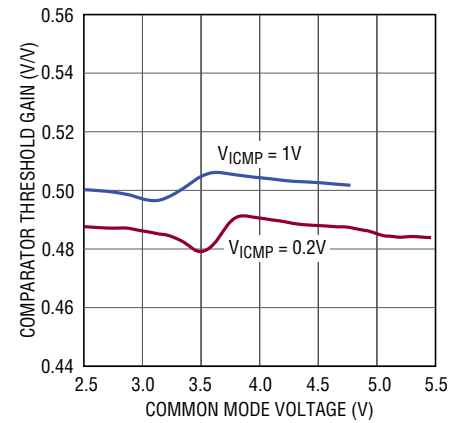
680412 G48

**isoSPI Driver Current Gain (Port A/Port B) vs Temperature**


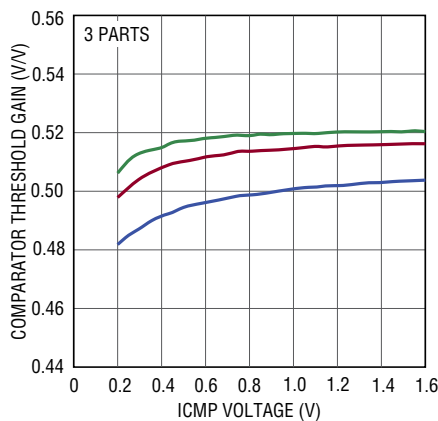
680412 G49

**isoSPI Driver Common Mode Voltage (Port A/Port B) vs Pulse Amplitude**


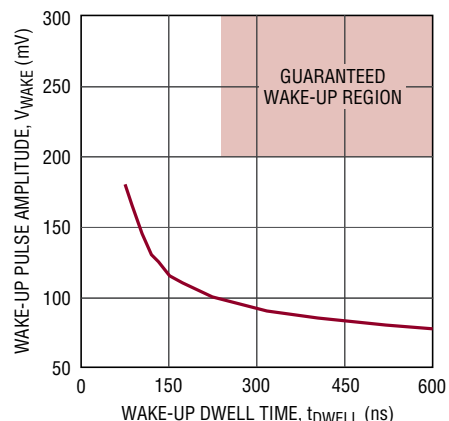
680412 G50

**isoSPI Comparator Threshold Gain (Port A/Port B) vs Common Mode**


680412 G51

**isoSPI Comparator Threshold Gain (Port A/Port B) vs ICMP Voltage**


680412 G52

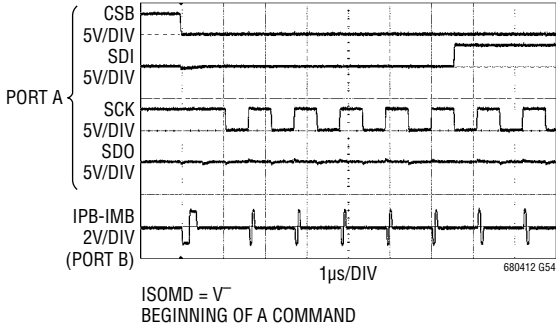
**Typical Wake-Up Pulse Amplitude (Port A) vs Dwell Time**


680412 G53

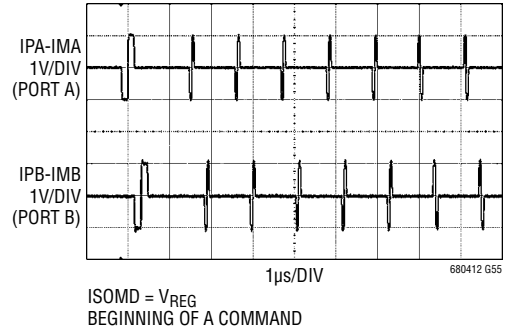
680412fc

## TYPICAL PERFORMANCE CHARACTERISTICS $T_A = 25^\circ\text{C}$ , unless otherwise noted.

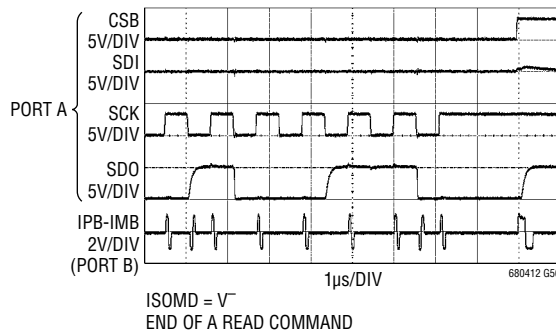
**Write Command to a Daisy-Chained Device (ISOMD = 0)**



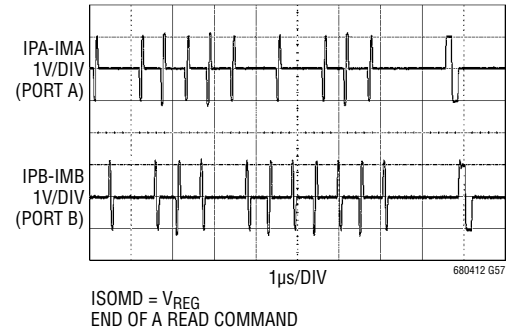
**Write Command to a Daisy-Chained Device (ISOMD = 1)**



**Data Read-Back from a Daisy-Chained Device (ISOMD = 0)**



**Data Read-Back from a Daisy-Chained Device (ISOMD = 1)**





## PIN FUNCTIONS

**C0 to C12:** Cell Inputs.

**S1 to S12:** Balance Inputs/Outputs. 12 N-MOSFETs are connected between S(n) and C(n – 1) for discharging cells.

**V<sup>+</sup>:** Positive Supply Pin.

**V<sup>-</sup>:** Negative Supply Pins. The V<sup>-</sup> pins must be shorted together, external to the IC.

**V<sub>REF2</sub>:** Buffered 2nd reference voltage for driving multiple 10k thermistors. Bypass with an external 1μF capacitor.

**V<sub>REF1</sub>:** ADC Reference Voltage. Bypass with an external 1μF capacitor. No DC loads allowed.

**GPIO[1:5]:** General Purpose I/O. Can be used as digital inputs or digital outputs, or as analog inputs with a measurement range from V<sup>-</sup> to 5V. GPIO [3:5] can be used as an I<sup>2</sup>C or SPI port.

**SWTEN:** Software Timer Enable. Connect this pin to V<sub>REG</sub> to enable the software timer.

**DRIVE:** Connect the base of an NPN to this pin. Connect the collector to V<sup>+</sup> and the emitter to V<sub>REG</sub>.

**V<sub>REG</sub>:** 5V Regulator Input. Bypass with an external 1μF capacitor.

**ISOMD:** Serial Interface Mode. Connecting ISOMD to V<sub>REG</sub> configures Pins 41 to 44 of the LTC6804 for 2-wire isolated interface (isoSPI) mode. Connecting ISOMD to V<sup>-</sup> configures the LTC6804 for 4-wire SPI mode.

**WDT:** Watchdog Timer Output Pin. This is an open drain NMOS digital output. It can be left unconnected or connected with a 1M resistor to V<sub>REG</sub>. If the LTC6804 does not receive a wake-up signal (see Figure 21) within 2 seconds, the watchdog timer circuit will reset the LTC6804 and the WDT pin will go high impedance.

### Serial Port Pins

	LTC6804-1 (DAISY-CHAINABLE)		LTC6804-2 (ADDRESSABLE)	
	ISOMD = V <sub>REG</sub>	ISOMD = V <sup>-</sup>	ISOMD = V <sub>REG</sub>	ISOMD = V <sup>-</sup>
PORT B (Pins 45 to 48)	IPB	IPB	A3	A3
	IMB	IMB	A2	A2
	ICMP	ICMP	A1	A1
	IBIAS	IBIAS	A0	A0
PORT A (Pins 41 to 44)	(NC)	SDO	IBIAS	SDO
	(NC)	SDI	ICMP	SDI
	IPA	SCK	IPA	SCK
	IMA	CSB	IMA	CSB

**CSB, SCK, SDI, SDO:** 4-Wire Serial Peripheral Interface (SPI). Active low chip select (CSB), serial clock (SCK), and serial data in (SDI) are digital inputs. Serial data out (SDO) is an open drain NMOS output pin. SDO requires a 5k pull-up resistor.

**A0 to A3:** Address Pins. These digital inputs are connected to V<sub>REG</sub> or V<sup>-</sup> to set the chip address for addressable serial commands.

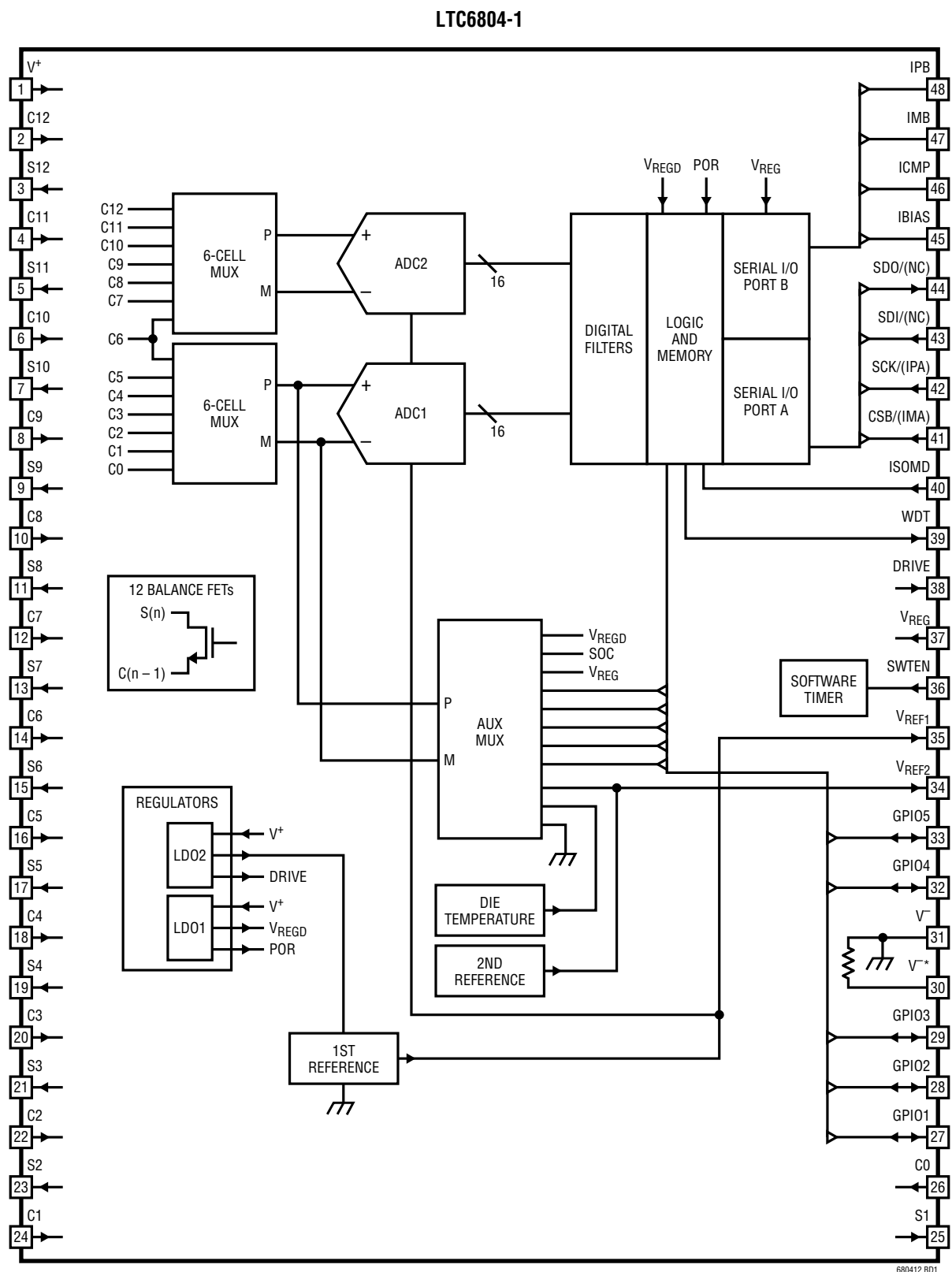
**IPA, IMA:** Isolated 2-Wire Serial Interface Port A. IPA (plus) and IMA (minus) are a differential input/output pair.

**IPB, IMB:** Isolated 2-Wire Serial Interface Port B. IPB (plus) and IMB (minus) are a differential input/output pair.

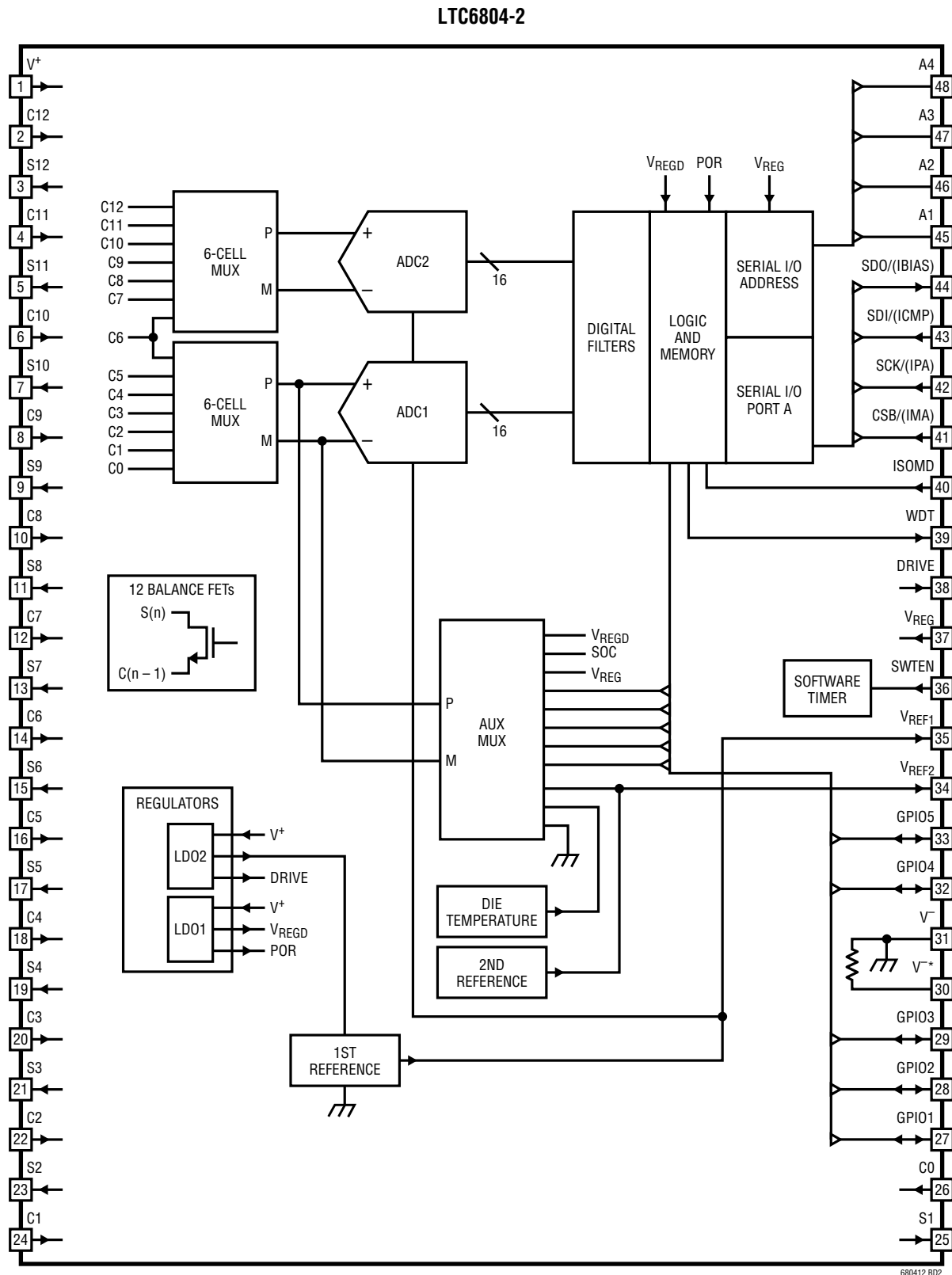
**IBIAS:** Isolated Interface Current Bias. Tie IBIAS to V<sup>-</sup> through a resistor divider to set the interface output current level. When the isoSPI interface is enabled, the IBIAS pin voltage is 2V. The IPA/IMA or IPB/IMB output current drive is set to 20 times the current, I<sub>B</sub>, sourced from the IBIAS pin.

**ICMP:** Isolated Interface Comparator Voltage Threshold Set. Tie this pin to the resistor divider between IBIAS and V<sup>-</sup> to set the voltage threshold of the isoSPI receiver comparators. The comparator thresholds are set to 1/2 the voltage on the ICMP pin.

BLOCK DIAGRAM



## BLOCK DIAGRAM



## OPERATION

### STATE DIAGRAM

The operation of the LTC6804 is divided into two separate sections: the core circuit and the isoSPI circuit. Both sections have an independent set of operating states, as well as a shutdown timeout.

### LTC6804 CORE STATE DESCRIPTIONS

#### SLEEP State

The reference and ADCs are powered down. The watchdog timer (see Watchdog and Software Discharge Timer) has timed out. The software discharge timer is either disabled or timed out. The supply currents are reduced to minimum levels. The isoSPI ports will be in the IDLE state.

If a WAKEUP signal is received (see Waking Up the Serial Interface), the LTC6804 will enter the STANDBY state.

#### STANDBY State

The reference and the ADCs are off. The watchdog timer and/or the software discharge timer is running. The DRIVE pin powers the  $V_{REG}$  pin to 5V through an external transistor. (Alternatively,  $V_{REG}$  can be powered by an external supply).

When a valid ADC command is received or the REFON bit is set to 1 in the Configuration Register Group, the IC pauses for  $t_{REFUP}$  to allow for the reference to power up and then enters either the REFUP or MEASURE state. If there is no WAKEUP signal for a duration  $t_{SLEEP}$  (when both the watchdog and software discharge timer have expired) the LTC6804

returns to the SLEEP state. If the software discharge timer is disabled, only the watchdog timer is relevant.

#### REFUP State

To reach this state the REFON bit in the Configuration Register Group must be set to 1 (using the WRCFG command, see Table 36). The ADCs are off. The reference is powered up so that the LTC6804 can initiate ADC conversions more quickly than from the STANDBY state.

When a valid ADC command is received, the IC goes to the MEASURE state to begin the conversion. Otherwise, the LTC6804 will return to the STANDBY state when the REFON bit is set to 0, either manually (using WRCFG command) or automatically when the watchdog timer expires. (The LTC6804 will then move straight into the SLEEP state if both timers are expired).

#### MEASURE State

The LTC6804 performs ADC conversions in this state. The reference and ADCs are powered up.

After ADC conversions are complete the LTC6804 will transition to either the REFUP or STANDBY states, depending on the REFON bit. Additional ADC conversions can be initiated more quickly by setting REFON = 1 to take advantage of the REFUP state.

Note: Non-ADC commands do not cause a Core state transition. Only an ADC conversion or diagnostic commands will place the Core in the MEASURE state.

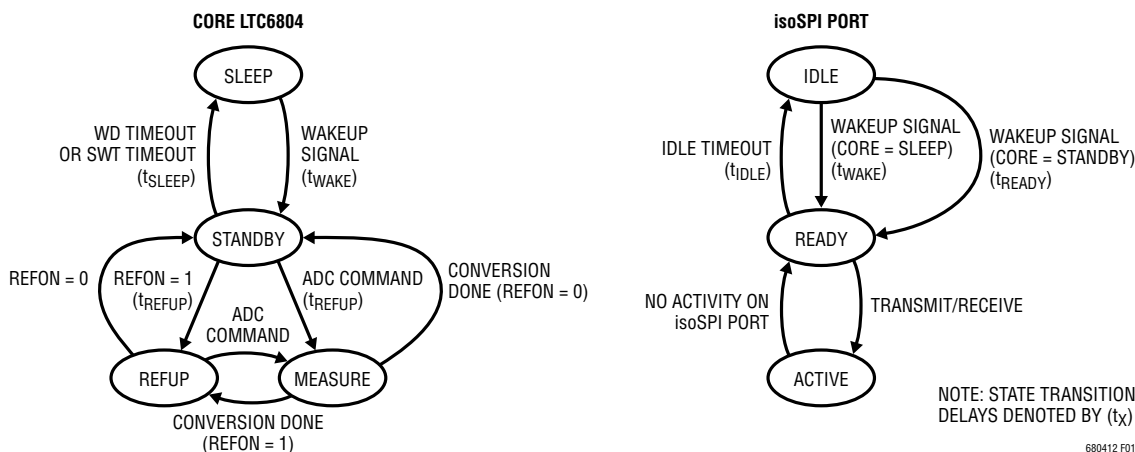


Figure 1. LTC6804 Operation State Diagram

## OPERATION

### isoSPI STATE DESCRIPTIONS

Note: The LTC6804-1 has two isoSPI ports (A and B), for daisy-chain communication. The LTC6804-2 has only one isoSPI port (A), for parallel-addressable communication.

#### IDLE State

The isoSPI ports are powered down.

When isoSPI port A receives a WAKEUP signal (see Waking Up the Serial Interface), the isoSPI enters the READY state. This transition happens quickly (within  $t_{\text{READY}}$ ) if the Core is in the STANDBY state because the DRIVE and  $V_{\text{REG}}$  pins are already biased up. If the Core is in the SLEEP state when the isoSPI receives a WAKEUP signal, then it transitions to the READY state within  $t_{\text{WAKE}}$ .

#### READY State

The isoSPI port(s) are ready for communication. Port B is enabled only for LTC6804-1, and is not present on the LTC6804-2. The serial interface current in this state depends on if the part is LTC6804-1 or LTC6804-2, the status of the ISOMD pin, and  $R_{\text{BIAS}} = R_{\text{B1}} + R_{\text{B2}}$  (the external resistors tied to the IBIAS pin).

If there is no activity (i.e., no WAKEUP signal) on port A for greater than  $t_{\text{IDLE}} = 5.5\text{ms}$ , the LTC6804 goes to the IDLE state. When the serial interface is transmitting or receiving data the LTC6804 goes to the ACTIVE state.

#### ACTIVE State

The LTC6804 is transmitting/receiving data using one or both of the isoSPI ports. The serial interface consumes maximum power in this state. The supply current increases with clock frequency as the density of isoSPI pulses increases.

### POWER CONSUMPTION

The LTC6804 is powered via two pins:  $V^+$  and  $V_{\text{REG}}$ . The  $V^+$  input requires voltage greater than or equal to the top cell voltage, and it provides power to the high voltage elements of the core circuitry. The  $V_{\text{REG}}$  input requires 5V and provides power to the remaining core circuitry and the isoSPI circuitry. The  $V_{\text{REG}}$  input can be powered through an external transistor, driven by the regulated

DRIVE output pin. Alternatively,  $V_{\text{REG}}$  can be powered by an external supply.

The power consumption varies according to the operational states. Table 1 and Table 2 provide equations to approximate the supply pin currents in each state. The  $V^+$  pin current depends only on the Core state and not on the isoSPI state. However, the  $V_{\text{REG}}$  pin current depends on both the Core state and isoSPI state, and can therefore be divided into two components. The isoSPI interface draws current only from the  $V_{\text{REG}}$  pin.

$$I_{\text{REG}} = I_{\text{REG(CORE)}} + I_{\text{REG(isoSPI)}}$$

**Table 1. Core Supply Current**

STATE		$I_{V^+}$	$I_{\text{REG(CORE)}}$
SLEEP	$V_{\text{REG}} = 0\text{V}$	$3.8\mu\text{A}$	$0\mu\text{A}$
	$V_{\text{REG}} = 5\text{V}$	$1.6\mu\text{A}$	$2.2\mu\text{A}$
STANDBY		$32\mu\text{A}$	$35\mu\text{A}$
REFUP		$550\mu\text{A}$	$450\mu\text{A}$
MEASURE		$550\mu\text{A}$	$11.5\text{mA}$

In the SLEEP state the  $V_{\text{REG}}$  pin will draw approximately  $2.2\mu\text{A}$  if powered by a external supply. Otherwise, the  $V^+$  pin will supply the necessary current.

### ADC OPERATION

There are two ADCs inside the LTC6804. The two ADCs operate simultaneously when measuring twelve cells. Only one ADC is used to measure the general purpose inputs. The following discussion uses the term ADC to refer to one or both ADCs, depending on the operation being performed. The following discussion will refer to ADC1 and ADC2 when it is necessary to distinguish between the two circuits, in timing diagrams, for example.

#### ADC Modes

The ADCOPT bit (CFGRO[0]) in the configuration register group and the mode selection bits MD[1:0] in the conversion command together provide 6 modes of operation for the ADC which correspond to different over sampling ratios (OSR). The accuracy of these modes are summarized in Table 3. In each mode, the ADC first measures the inputs, and then performs a calibration of each channel. The names of the modes are based on the  $-3\text{dB}$  bandwidth of the ADC measurement.

## OPERATION

**Table 2. isoSPI Supply Current Equations**

isoSPI STATE	DEVICE	ISOMD CONNECTION	$I_{REG(ISO SPI)}$
IDLE	LTC6804-1/LTC6804-2	N/A	0mA
READY	LTC6804-1	$V_{REG}$	$2.8mA + 5 \cdot I_B$ Note: $I_B = V_{BIAS}/(R_{B1} + R_{B2})$
		$V^-$	$1.6mA + 3 \cdot I_B$
	LTC6804-2	$V_{REG}$	$1.8mA + 3 \cdot I_B$
		$V^-$	0mA
ACTIVE	LTC6804-1	$V_{REG}$	Write: $2.8mA + 5 \cdot I_B + (2 \cdot I_B + 0.4mA) \cdot \frac{1\mu s}{t_{CLK}}$ Read: $2.8mA + 5 \cdot I_B + (3 \cdot I_B + 0.5mA) \cdot \frac{1\mu s}{t_{CLK}}$
		$V^-$	$1.6mA + 3 \cdot I_B + (2 \cdot I_B + 0.2mA) \cdot \frac{1\mu s}{t_{CLK}}$
	LTC6804-2	$V_{REG}$	Write: $1.8mA + 3 \cdot I_B + (0.3mA) \cdot \frac{1\mu s}{t_{CLK}}$ Read: $1.8mA + 3 \cdot I_B + (I_B + 0.3mA) \cdot \frac{1\mu s}{t_{CLK}}$
		$V^-$	0mA

**Table 3. ADC Filter Bandwidth and Accuracy**

MODE	–3dB FILTER BW	–40dB FILTER BW	TME SPEC AT 3.3V, 25°C	TME SPEC AT 3.3V, –40°C, 125°C
27kHz (Fast Mode)	27kHz	84kHz	±4.7mV	±4.7mV
14kHz	13.5kHz	42kHz	±4.7mV	±4.7mV
7kHz (Normal Mode)	6.8kHz	21kHz	±1.2mV	±2.2mV
3kHz	3.4kHz	10.5kHz	±1.2mV	±2.2mV
2kHz	1.7kHz	5.3kHz	±1.2mV	±2.2mV
26Hz (Filtered Mode)	26Hz	82Hz	±1.2mV	±2.2mV

Note: TME is the total measurement error.

### Mode 7kHz (Normal):

In this mode, the ADC has high resolution and low TME (total measurement error). This is considered the normal operating mode because of the optimum combination of speed and accuracy.

### Mode 27kHz (Fast):

In this mode, the ADC has maximum throughput but has some increase in TME (total measurement error). So this mode is also referred to as the fast mode. The increase in speed comes from a reduction in the oversampling ratio. This results in an increase in noise and average measurement error.

### Mode 26Hz (Filtered):

In this mode, the ADC digital filter –3dB frequency is lowered to 26Hz by increasing the OSR. This mode is also referred to as the filtered mode due to its low –3dB frequency. The accuracy is similar to the 7kHz (Normal) mode with lower noise.

### Modes 14kHz, 3kHz and 2kHz:

Modes 14kHz, 3kHz and 2kHz provide additional options to set the ADC digital filter –3dB frequency at 13.5kHz, 3.4kHz and 1.7kHz respectively. The accuracy of the 14kHz mode is similar to the 27kHz (fast) mode. The accuracy of 3kHz and 2kHz modes is similar to the 7kHz (normal) mode.

680412fc

## OPERATION

The conversion times for these modes are provided in Table 5. If the core is in STANDBY state, an additional  $t_{REFUP}$  time is required to power up the reference before beginning the ADC conversions. The reference can remain powered up between ADC conversions if the REFON bit in Configuration Register Group is set to 1 so the core is in REFUP state after a delay  $t_{REFUP}$ . Then, the subsequent ADC commands will not have the  $t_{REFUP}$  delay before beginning ADC conversions.

### ADC Range and Resolution

The C inputs and GPIO inputs have the same range and resolution. The ADC inside the LTC6804 has an approximate range from  $-0.82V$  to  $5.73V$ . Negative readings are rounded to  $0V$ . The format of the data is a 16-bit unsigned integer where the LSB represents  $100\mu V$ . Therefore, a reading of  $0x80E8$  (33,000 decimal) indicates a measurement of  $3.3V$ .

Delta-Sigma ADCs have quantization noise which depends on the input voltage, especially at low over sampling ratios (OSR), such as in FAST mode. In some of the ADC modes, the quantization noise increases as the input voltage approaches the upper and lower limits of the ADC range. For example, the total measurement noise versus input voltage in normal and filtered modes is shown in Figure 2.

The specified range of the ADC is  $0V$  to  $5V$ . In Table 4, the precision range of the ADC is arbitrarily defined as  $0.5V$  to  $4.5V$ . This is the range where the quantization noise is relatively constant even in the lower OSR modes (see Figure 2). Table 4 summarizes the total noise in this range for all six ADC operating modes. Also shown is the noise

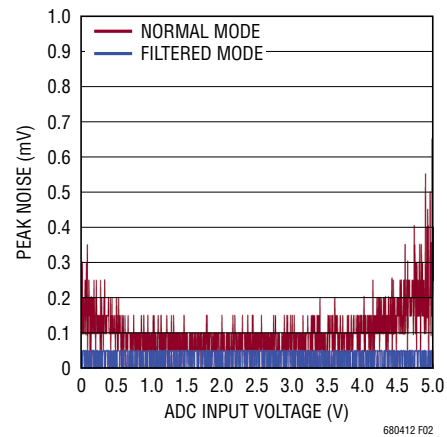


Figure 2. Measurement Noise vs Input Voltage

free resolution. For example, 14-bit noise free resolution in normal mode implies that the top 14 bits will be noise free with a DC input, but that the 15th and 16th least significant bits (LSB) will flicker.

### ADC Range vs Voltage Reference Value:

Typical Delta-Sigma ADC's have a range which is exactly twice the value of the voltage reference, and the ADC measurement error is directly proportional to the error in the voltage reference. The LTC6804 ADC is not typical. The absolute value of  $V_{REF1}$  is trimmed up or down to compensate for gain errors in the ADC. Therefore, the ADC total measurement error (TME) specifications are superior to the  $V_{REF1}$  specifications. For example, the  $25^{\circ}C$  specification of the total measurement error when measuring  $3.300V$  in  $7kHz$  (normal) mode is  $\pm 1.2mV$  and the  $25^{\circ}C$  specification for  $V_{REF1}$  is  $3.200V \pm 100mV$ .

Table 4. ADC Range and Resolution

MODE	FULL RANGE <sup>1</sup>	SPECIFIED RANGE	PRECISION RANGE <sup>2</sup>	LSB	FORMAT	MAX NOISE	NOISE FREE RESOLUTION <sup>3</sup>
27kHz (Fast)	$-0.8192V$ to $5.7344V$	$0V$ to $5V$	$0.5V$ to $4.5V$	$100\mu V$	Unsigned 16 Bits	$\pm 4mV_{p-p}$	10 Bits
14kHz						$\pm 1mV_{p-p}$	12 Bits
7kHz (Normal)						$\pm 250\mu V_{p-p}$	14 Bits
3kHz						$\pm 150\mu V_{p-p}$	14 Bits
2kHz						$\pm 100\mu V_{p-p}$	15 Bits
26Hz (Filtered)						$\pm 50\mu V_{p-p}$	16 Bits

1. Negative readings are rounded to  $0V$ .

2. PRECISION RANGE is the range over which the noise is less than MAX NOISE.

3. NOISE FREE RESOLUTION is a measure of the noise level within the PRECISION RANGE.



## OPERATION

### Measuring Cell Voltages (ADCV Command)

The ADCV command initiates the measurement of the battery cell inputs, pins C0 through C12. This command has options to select the number of channels to measure and the ADC mode. See the section on Commands for the ADCV command format.

Figure 3 illustrates the timing of ADCV command which measures all twelve cells. After the receipt of the ADCV command to measure all 12 cells, ADC1 sequentially measures the bottom 6 cells. ADC2 sequentially measures the top 6 cells. After the cell measurements are complete, each channel is calibrated to remove any offset errors.

Table 5 shows the conversion times for the ADCV command measuring all 12 cells. The total conversion time is given by  $t_{6C}$  which indicates the end of the calibration step.

Figure 4 illustrates the timing of the ADCV command that measures only two cells.

Table 6 shows the conversion time for ADCV command measuring only 2 cells.  $t_{1C}$  indicates the total conversion time for this command.

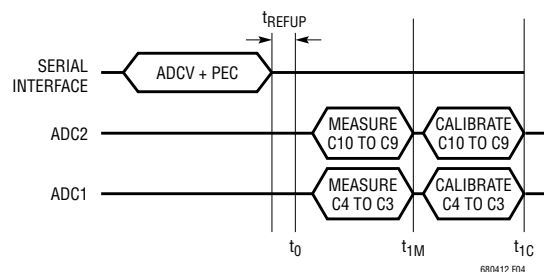


Figure 4. Timing for ADCV Command Measuring 2 Cells

Table 6. Conversion Times for ADCV Command Measuring Only 2 Cells in Different Modes

MODE	CONVERSION TIMES (in $\mu s$ )		
	$t_0$	$t_{1M}$	$t_{1C}$
27kHz	0	57	201
14kHz	0	86	230
7kHz	0	144	405
3kHz	0	260	521
2kHz	0	493	754
26Hz	0	29,817	33,568

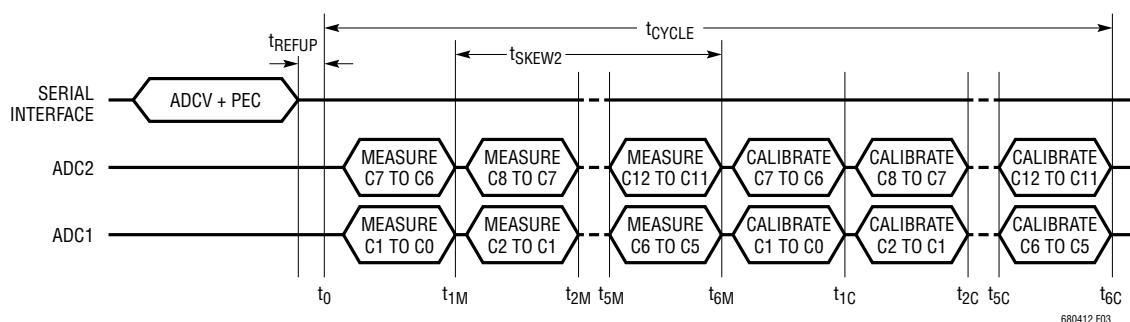


Figure 3. Timing for ADCV Command Measuring All 12 Cells

Table 5. Conversion Times for ADCV Command Measuring All 12 Cells in Different Modes

MODE	CONVERSION TIMES (in $\mu s$ )								
	$t_0$	$t_{1M}$	$t_{2M}$	$t_{5M}$	$t_{6M}$	$t_{1C}$	$t_{2C}$	$t_{5C}$	$t_{6C}$
27kHz	0	57	103	243	290	432	568	975	1,113
14kHz	0	86	162	389	465	606	742	1,149	1,288
7kHz	0	144	278	680	814	1,072	1,324	2,080	2,335
3kHz	0	260	511	1,262	1,512	1,770	2,022	2,778	3,033
2kHz	0	493	976	2,425	2,908	3,166	3,418	4,175	4,430
26Hz	0	29,817	59,623	149,043	178,850	182,599	186,342	197,571	201,317



## OPERATION

### Under/Overvoltage Monitoring

Whenever the C inputs are measured, the results are compared to undervoltage and overvoltage thresholds stored in memory. If the reading of a cell is above the overvoltage limit, a bit in memory is set as a flag. Similarly, measurement results below the undervoltage limit cause a flag to be set. The overvoltage and undervoltage thresholds are stored in the configuration register group. The flags are stored in the status register group B.

### Auxiliary (GPIO) Measurements (ADAX Command)

The ADAX command initiates the measurement of the GPIO inputs. This command has options to select which GPIO input to measure (GPIO1-5) and which ADC mode. The ADAX command also measures the 2nd reference. There are options in the ADAX command to measure each GPIO and the 2nd reference separately or to measure all 5 GPIOs and the 2nd reference in a single command. See the section on commands for the ADAX command format. All auxiliary measurements are relative to the  $V^-$  pin voltage. This command can be used to read external temperature

by connecting the temperature sensors to the GPIOs. These sensors can be powered from the 2nd reference which is also measured by the ADAX command, resulting in precise ratiometric measurements.

Figure 5 illustrates the timing of the ADAX command measuring all GPIOs and the 2nd reference. Since all the 6 measurements are carried out on ADC1 alone, the conversion time for the ADAX command is similar to the ADCV command.

### Measuring Cell Voltages and GPIOs (ADCVAX Command)

The ADCVAX command combines twelve cell measurements with two GPIO measurements (GPIO1 and GPIO2). This command simplifies the synchronization of battery cell voltage and current measurements when current sensors are connected to GPIO1 or GPIO2 inputs. Figure 6 illustrates the timing of the ADCVAX command. See the section on commands for the ADCVAX command format. The synchronization of the current and voltage measurements,  $t_{SKEW1}$ , in FAST MODE is within 208 $\mu$ s.

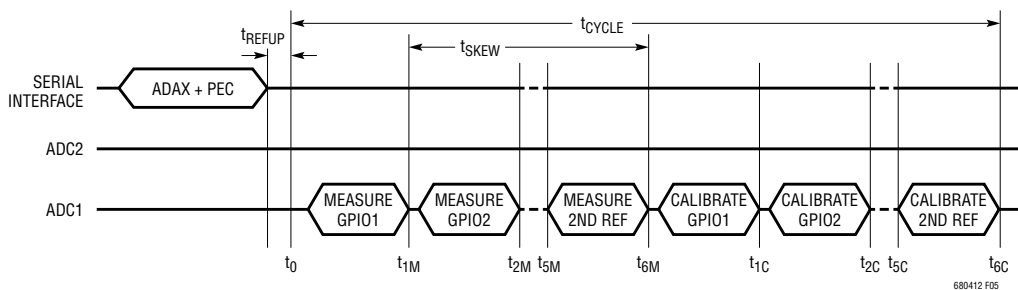


Figure 5. Timing for ADAX Command Measuring All GPIOs and 2nd Reference

Table 7. Conversion Times for ADAX Command Measuring All GPIOs and 2nd Reference in Different Modes

MODE	CONVERSION TIMES (in $\mu$ s)								
	$t_0$	$t_{1M}$	$t_{2M}$	$t_{5M}$	$t_{6M}$	$t_{1C}$	$t_{2C}$	$t_{5C}$	$t_{6C}$
27kHz	0	57	103	243	290	432	568	975	1,113
14kHz	0	86	162	389	465	606	742	1,149	1,288
7kHz	0	144	278	680	814	1,072	1,324	2,080	2,335
3kHz	0	260	511	1,262	1,512	1,770	2,022	2,778	3,033
2kHz	0	493	976	2,425	2,908	3,166	3,418	4,175	4,430
26Hz	0	29,817	59,623	149,043	178,850	182,599	186,342	197,571	201,317

## OPERATION

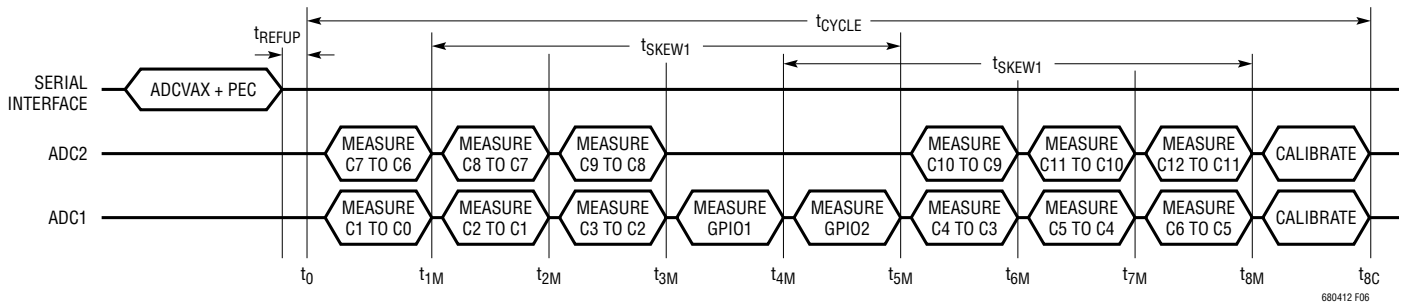


Figure 6. Timing of ADCVAX Command

Table 8. Conversion and Synchronization Times for ADCVAX Command in Different Modes

MODE	CONVERSION TIMES (in $\mu$ s)										SYNCHRONIZATION TIME ( $\mu$ s)
	$t_0$	$t_{1M}$	$t_{2M}$	$t_{3M}$	$t_{4M}$	$t_{5M}$	$t_{6M}$	$t_{7M}$	$t_{8M}$	$t_{8C}$	$t_{SKEW1}$
27kHz	0	57	106	155	216	265	326	375	424	1,564	208
14kHz	0	86	161	237	320	396	479	555	630	1,736	310
7kHz	0	144	278	412	553	687	828	962	1,096	3,133	543
3kHz	0	260	511	761	1,018	1,269	1,526	1,777	2,027	4,064	1009
2kHz	0	493	976	1,459	1,949	2,432	2,923	3,406	3,888	5,925	1939
26Hz	0	29,817	59,623	89,430	119,244	149,051	178,864	208,671	238,478	268,442	119234

Table 8 shows the conversion and synchronization time for the ADCVAX command in different modes. The total conversion time for the command is given by  $t_{8C}$ .

### DATA ACQUISITION SYSTEM DIAGNOSTICS

The battery monitoring data acquisition system is comprised of the multiplexers, ADCs, 1st reference, digital filters, and memory. To ensure long term reliable performance there are several diagnostic commands which can be used to verify the proper operation of these circuits.

### Measuring Internal Device Parameters (ADSTAT Command)

The ADSTAT command is a diagnostic command that measures the following internal device parameters: sum of all cells (SOC), internal die temperature (ITMP), analog power supply (VA) and the digital power supply (VD). These parameters are described in the section below. All 6 ADC modes are available for these conversions. See the section on commands for the ADSTAT command format. Figure 7 illustrates the timing of the ADSTAT command measuring all 4 internal device parameters.

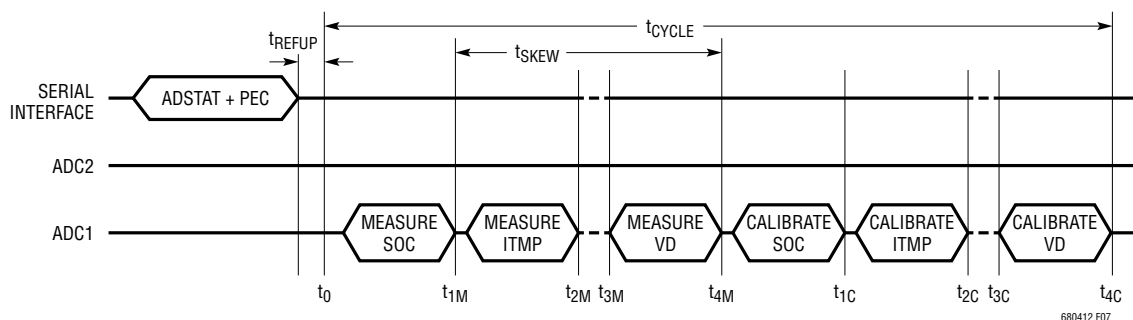


Figure 7. Timing for ADSTAT Command Measuring SOC, ITMP, VA, VD

## OPERATION

Table 9 shows the conversion time of the ADSTAT command measuring all 4 internal parameters.  $t_{4c}$  indicates the total conversion time for the ADSTAT command.

**Sum of Cells Measurement:** The sum of all cells measurement is the voltage between C12 and C0 with a 20:1 attenuation. The 16-bit ADC value of sum of cells measurement (SOC) is stored in status register group A. Any potential difference between the C0 and  $V^-$  pins results in an error in the SOC measurement equal to this difference. From the SOC value, the sum of all cell voltage measurements is given by:

$$\text{Sum of all Cells} = \text{SOC} \cdot 20 \cdot 100\mu\text{V}$$

**Internal Die Temperature:** The ADSTAT command can measure the internal die temperature. The 16-bit ADC value of the die temperature measurement (ITMP) is stored in status register group A. From ITMP the actual die temperature is calculated using the expression:

$$\text{Internal Die Temperature } (^{\circ}\text{C}) = (\text{ITMP}) \cdot 100\mu\text{V} / (7.5\text{mV})^{\circ}\text{C} - 273^{\circ}\text{C}$$

**Power Supply Measurements:** The ADSTAT command is also used to measure the analog power supply ( $V_{\text{REG}}$ ) and digital power supply ( $V_{\text{REGD}}$ ).

The 16-bit ADC value of the analog power supply measurement (VA) is stored in Status Register Group A. The 16-bit ADC value of the digital power supply measurement (VD) is stored in status register group B. From VA and VD, the power supply measurements are given by:

$$\text{Analog power supply measurement } (V_{\text{REG}}) = V_A \cdot 100\mu\text{V}$$

$$\text{Digital power supply measurement } (V_{\text{REGD}}) = V_D \cdot 100\mu\text{V}$$

The nominal range of  $V_{\text{REG}}$  is 4.5V to 5.5V. The nominal range of  $V_{\text{REGD}}$  is 2.7V to 3.6V.

Issuing an ADSTAT command with CHST = 100 runs an ADC measurement of just the digital supply ( $V_{\text{REGD}}$ ). This is not recommended following an ADCV command. With large cell voltages, running the ADSTAT command with CST = 100 following an ADCV command with CH = 000 (all cells) can cause the LTC6804 to perform a power on reset. If using the ADSTAT command with CHST = 100, it is necessary to run an ADCV command with CH = 001 prior to running the ADSTAT command with CHST = 100. This charges the high voltage multiplexer to a low potential before the  $V_{\text{REGD}}$  measurement is executed. To save time, this sacrificial ADCV command run prior to running the  $V_{\text{REGD}}$  measurement can be executed in FAST mode (MD = 01).

### Accuracy Check

Measuring an independent voltage reference is the best means to verify the accuracy of a data acquisition system. The LTC6804 contains a 2nd reference for this purpose. The ADAX command will initiate the measurement of the 2nd reference. The results are placed in auxiliary register group B. The range of the result depends on the ADC measurement accuracy and the accuracy of the 2nd reference, including thermal hysteresis and long term drift. Readings outside the range 2.985 to 3.015 indicate the system is out of its specified tolerance.

### MUX Decoder Check

The diagnostic command DIAGN ensures the proper operation of each multiplexer channel. The command cycles through all channels and sets the MUXFAIL bit to 1 in status register group B if any channel decoder fails. The MUXFAIL bit is set to 0 if the channel decoder passes the

**Table 9. Conversion Times for ADSTAT Command Measuring SOC, ITMP, VA, VD**

MODE	CONVERSION TIMES (in $\mu\text{s}$ )								
	$t_0$	$t_{1M}$	$t_{2M}$	$t_{3M}$	$t_{4M}$	$t_{1c}$	$t_{2c}$	$t_{3c}$	$t_{4c}$
27kHz	0	57	103	150	197	338	474	610	748
14kHz	0	86	162	237	313	455	591	726	865
7kHz	0	144	278	412	546	804	1,056	1,308	1,563
3kHz	0	260	511	761	1,011	1,269	1,522	1,774	2,028
2kHz	0	493	976	1,459	1,942	2,200	2,452	2,705	2,959
26Hz	0	29,817	59,623	89,430	119,237	122,986	126,729	130,472	134,218

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test. The MUXFAIL bit is also set to 1 on power-up (POR) or after a CLRSTAT command.

The DIAGN command takes about 400 $\mu$ s to complete if the core is in REFUP state and about 4.5ms to complete if the core is in STANDBY state. The polling methods described in the section Polling Methods can be used to determine the completion of the DIAGN command.

### Digital Filter Check

The delta-sigma ADC is composed of a 1-bit pulse density modulator followed by a digital filter. A pulse density modulated bit stream has a higher percentage of 1s for higher analog input voltages. The digital filter converts this high frequency 1-bit stream into a single 16-bit word. This is why a delta-sigma ADC is often referred to as an oversampling converter.

The self test commands verify the operation of the digital filters and memory. Figure 8 illustrates the operation of the ADC during self test. The output of the 1-bit pulse density modulator is replaced by a 1-bit test signal. The

test signal passes through the digital filter and is converted to a 16-bit value. The 1-bit test signal undergoes the same digital conversion as the regular 1-bit pulse from the modulator, so the conversion time for any self test command is exactly the same as the corresponding regular ADC conversion command. The 16-bit ADC value is stored in the same register groups as the regular ADC conversion command. The test signals are designed to place alternating one-zero patterns in the registers. Table 10 provides a list of the self test commands. If the digital filters and memory are working properly, then the registers will contain the values shown in Table 10. For more details see the section Commands.

### ADC Clear Commands

LTC6804 has 3 clear commands – CLRCELL, CLRAUX and CLRSTAT. These commands clear the registers that store all ADC conversion results.

The CLRCELL command clears cell voltage register group A, B, C and D. All bytes in these registers are set to 0xFF by CLRCELL command.

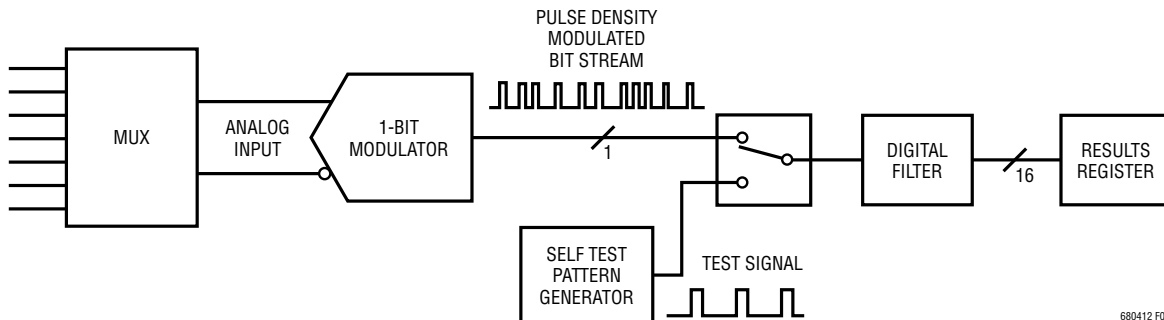


Figure 8. Operation of LTC6804 ADC Self Test

Table 10. Self Test Command Summary

COMMAND	SELF TEST OPTION	OUTPUT PATTERN IN DIFFERENT ADC MODES						RESULTS REGISTER GROUPS
		27kHz	14kHz	7kHz	3kHz	2kHz	26Hz	
CVST	ST[1:0]=01	0x9565	0x9553	0x9555	0x9555	0x9555	0x9555	C1V to C12V (CVA, CVB, CVC, CVD)
	ST[1:0]=10	0x6A9A	0x6AAC	0x6AAA	0x6AAA	0x6AAA	0x6AAA	
AXST	ST[1:0]=01	0x9565	0x9553	0x9555	0x9555	0x9555	0x9555	G1V to G5V, REF (AUXA, AUXB)
	ST[1:0]=10	0x6A9A	0x6AAC	0x6AAA	0x6AAA	0x6AAA	0x6AAA	
STATST	ST[1:0]=01	0x9565	0x9553	0x9555	0x9555	0x9555	0x9555	SOC, ITMP, VA, VD (STATA, STATB)
	ST[1:0]=10	0x6A9A	0x6AAC	0x6AAA	0x6AAA	0x6AAA	0x6AAA	

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The CLRAUX command clears auxiliary register group A and B. All bytes in these registers are set to 0xFF by CLRAUX command.

The CLRSTAT command clears status register group A and B except the REVCODE and RSVD bits in status register group B. A read back of REVCODE will return the revision code of the part. All OV flags, UV flags, MUXFAIL bit, and THSD bit in status register group B are set to 1 by CLRSTAT command. The THSD bit is set to 0 after RDSTATB command. The registers storing SOC, ITMP, VA and VD are all set to 0xFF by CLRSTAT command.

### Open-Wire Check (ADOW Command)

The ADOW command is used to check for any open wires between the ADCs in the LTC6804 and the external cells. This command performs ADC conversions on the C pin inputs identically to the ADCV command, except two internal current sources sink or source current into the two C pins while they are being measured. The pull-up (PUP) bit of the ADOW command determines whether the current sources are sinking or sourcing 100 $\mu$ A.

The following simple algorithm can be used to check for an open wire on any of the 13 C pins (see Figure 9):

- 1) Run the 12-cell command ADOW with PUP = 1 at least twice. Read the cell voltages for cells 1 through 12 once at the end and store them in array CELL<sub>PU</sub>(n).
- 2) Run the 12-cell command ADOW with PUP = 0 at least twice. Read the cell voltages for cells 1 through 12 once at the end and store them in array CELL<sub>PD</sub>(n).
- 3) Take the difference between the pull-up and pull-down measurements made in above steps for cells 2-12:  
 $CELL_{\Delta}(n) = CELL_{PU}(n) - CELL_{PD}(n)$ .
- 4) For all values of n from 1 to 11: If  $CELL_{\Delta}(n+1) < -400\text{mV}$ , then C(n) is open. If the  $CELL_{PU}(1) = 0.0000$ , then C(0) is open. If the  $CELL_{PD}(12) = 0.0000$ , then C(12) is open.

The above algorithm detects open wires using normal mode conversions with as much as 10nF of capacitance remaining on the LTC6804 side of the open wire. However, if more external capacitance is on the open C pin, then the length of time that the open wire conversions are ran in steps 1 and 2 must be increased to give the 100 $\mu$ A current sources

time to create a large enough difference for the algorithm to detect an open connection. This can be accomplished by running more than two ADOW commands in steps 1 and 2, or by using filtered mode conversions instead of normal mode conversions. Use Table 11 to determine how many conversions are necessary:

Table 11

EXTERNAL C PIN CAPACITANCE	Number of ADOW Commands Required in Steps 1 and 2	
	NORMAL MODE	FILTERED MODE
$\leq 10\text{nF}$	2	2
100nF	10	2
1 $\mu$ F	100	2
C	$1 + \text{ROUNDUP}(C/10\text{nF})$	2

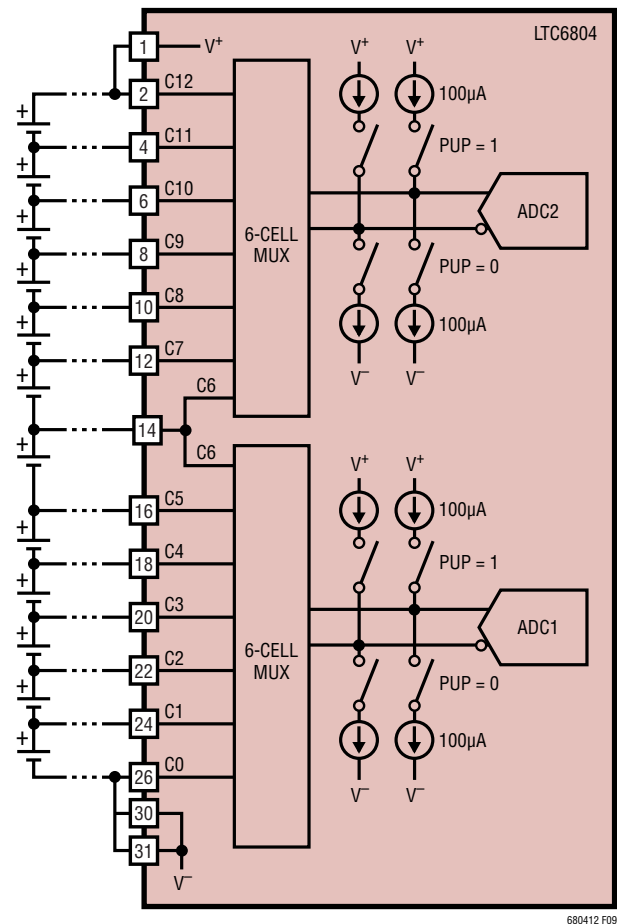


Figure 9. Open-Wire Detection Circuitry

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### Thermal Shutdown

To protect the LTC6804 from overheating, there is a thermal shutdown circuit included inside the IC. If the temperature detected on the die goes above approximately 150°C, the thermal shutdown circuit trips and resets the configuration register group to its default state. This turns off all discharge switches. When a thermal shutdown event has occurred, the THSD bit in status register group B will go high. This bit is cleared after a read operation has been performed on the status register group B (RDSTATB command). The CLRSTAT command sets the THSD bit high for diagnostic purposes, but does not reset the configuration register group.

### Revision Code and Reserved Bits

The status register group B contains a 4-bit revision code and 2 reserved bits. If software detection of device revision is necessary, then contact the factory for details. Otherwise, the code can be ignored. In all cases, however, the values of all bits must be used when calculating the packet error code (PEC) on data reads.

### WATCHDOG AND SOFTWARE DISCHARGE TIMER

When there is no wake-up signal (see Figure 21) for more than 2 seconds, the watchdog timer expires. This resets configuration register bytes CFGR0-CFGR3 in all cases. CFGR4 and CFGR5 are reset by the watchdog timer when the software timer is disabled. The WDT pin is pulled high by the external pull-up when the watchdog time elapses. The watchdog timer is always enabled and is reset by a qualified wake-up signal.

The software discharge timer is used to keep the discharge switches turned ON for programmable time duration. If the software timer is being used, the discharge switches are not turned OFF when the watchdog timer is activated.

To enable the software timer, SWTEN pin needs to be tied high to  $V_{REG}$  (Figure 10). The discharge switches can now be kept ON for the programmed time duration that is determined by the DCTO value written to the configuration register. Table 12 shows the various time settings and the corresponding DCTO value. Table 13 summarizes the status of the configuration register group after a watchdog timer or software timer event.

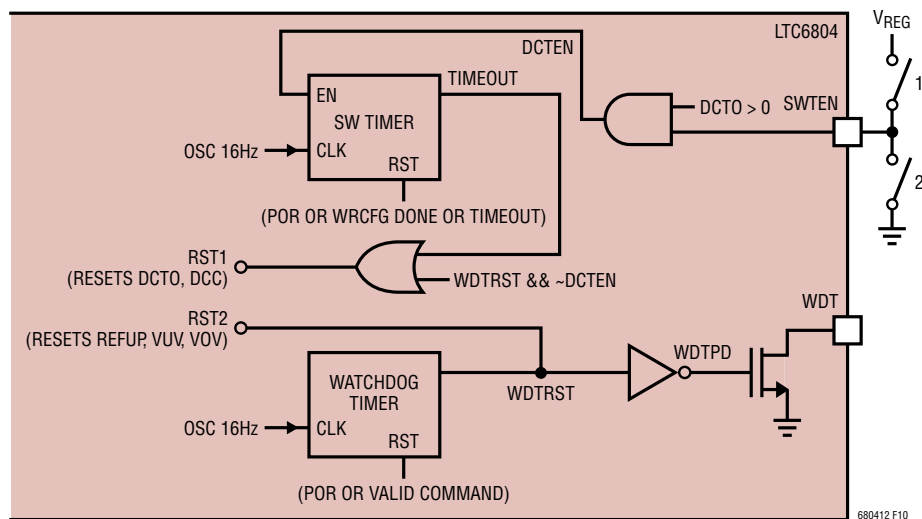


Figure 10. Watchdog and Software Discharge Timer

Table 12. DCTO Settings

DCTO	0	1	2	3	4	5	6	7	8	9	A	B	C	D	E	F
Time Min	Disabled	0.5	1	2	3	4	5	10	15	20	30	40	60	75	90	120



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Table 13

	WATCHDOG TIMER	SOFTWARE TIMER
SWTEN = 0, DCTO = XXXX	Resets CFGR0-5 When It Activates	Disabled
SWTEN = 1, DCTO = 0000	Resets CFGR0-5 When It Activates	Disabled
SWTEN = 1, DCTO ! = 0000	Resets CFGR0-3 When It Activates	Resets CFGR4-5 When It Fires

Unlike the watchdog timer, the software timer does not reset when there is a valid command. The software timer can only be reset after a valid WRCFG (write configuration register) command. There is a possibility that the software timer will expire in the middle of some commands.

If software timer activates in the middle of WRCFG command, the configuration register resets as per Table 14. However, at the end of the valid WRCFG command, the new data is copied to the configuration register. The new data is not lost when the software timer is activated.

If software timer activates in the middle of RDCFG command, the configuration register group resets as per Table 14. As a result, the read back data from bytes CRFG4 and CRFG5 could be corrupted.

### I<sup>2</sup>C/SPI MASTER ON LTC6804 USING GPIOs

The I/O ports GPIO3, GPIO4 and GPIO5 on LTC6804-1 and LTC6804-2 can be used as an I<sup>2</sup>C or SPI master port to communicate to an I<sup>2</sup>C or SPI slave. In the case of an I<sup>2</sup>C master, GPIO4 and GPIO5 form the SDA and SCL ports of the I<sup>2</sup>C interface respectively. In the case of a SPI master, GPIO3, GPIO5 and GPIO4 become the chip select (CSBM), clock (SCKM) and data (SDIOM) ports of the SPI interface respectively. The SPI master on LTC6804 supports only SPI mode 3 (CHPA = 1, CPOL = 1).

Table 14

DCTO (READ VALUE)	TIME LEFT (MIN)
0	Disabled (or) Timer Has Timed Out
1	$0 < \text{Timer} \leq 0.5$
2	$0.5 < \text{Timer} \leq 1$
3	$1 < \text{Timer} \leq 2$
4	$2 < \text{Timer} \leq 3$
5	$3 < \text{Timer} \leq 4$
6	$4 < \text{Timer} \leq 5$
7	$5 < \text{Timer} \leq 10$
8	$10 < \text{Timer} \leq 15$
9	$15 < \text{Timer} \leq 20$
A	$20 < \text{Timer} \leq 30$
B	$30 < \text{Timer} \leq 40$
C	$40 < \text{Timer} \leq 60$
D	$60 < \text{Timer} \leq 75$
E	$75 < \text{Timer} \leq 90$
F	$90 < \text{Timer} \leq 120$

The GPIOs are open drain outputs, so an external pull-up is required on these ports to operate as an I<sup>2</sup>C or SPI master. It is also important to write the GPIO bits to 1 in the CFG register group so these ports are not pulled low internally by the device.

### COMM Register

LTC6804 has a 6-byte COMM register as shown in Table 15. This register stores all data and control bits required for I<sup>2</sup>C or SPI communication to a slave. The COMM register contains 3 bytes of data Dn[7:0] to be transmitted to or received from the slave device. ICOMn [3:0] specify control actions before transmitting/receiving the data byte. FCOMn [3:0] specify control actions after transmitting/receiving the data byte.

Table 15. COMM Register Memory Map

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
COMM0	RD/WR	ICOM0[3]	ICOM0[2]	ICOM0[1]	ICOM0[0]	D0[7]	D0[6]	D0[5]	D0[4]
COMM1	RD/WR	D0[3]	D0[2]	D0[1]	D0[0]	FCOM0[3]	FCOM0[2]	FCOM0[1]	FCOM0[0]
COMM2	RD/WR	ICOM1[3]	ICOM1[2]	ICOM1[1]	ICOM1[0]	D1[7]	D1[6]	D1[5]	D1[4]
COMM3	RD/WR	D1[3]	D1[2]	D1[1]	D1[0]	FCOM1[3]	FCOM1[2]	FCOM1[1]	FCOM1[0]
COMM4	RD/WR	ICOM2[3]	ICOM2[2]	ICOM2[1]	ICOM2[0]	D2[7]	D2[6]	D2[5]	D2[4]
COMM5	RD/WR	D2[3]	D2[2]	D2[1]	D2[0]	FCOM2[3]	FCOM2[2]	FCOM2[1]	FCOM2[0]

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**Table 16. Write Codes for ICOMn[3:0] and FCOMn[3:0] on I<sup>2</sup>C Master**

CONTROL BITS	CODE	ACTION	DESCRIPTION
ICOMn[3:0]	0110	START	Generate a START Signal on I <sup>2</sup> C Port Followed By Data Transmission
	0001	STOP	Generate a STOP Signal on I <sup>2</sup> C port
	0000	BLANK	Proceed Directly to Data Transmission on I <sup>2</sup> C Port
	0111	No Transmit	Release SDA and SCL and Ignore the Rest of the Data
FCOMn[3:0]	0000	Master ACK	Master Generates an ACK Signal on Ninth Clock Cycle
	1000	Master NACK	Master Generates a NACK Signal on Ninth Clock Cycle
	1001	Master NACK + STOP	Master Generates a NACK Signal Followed by STOP Signal

**Table 17. Write Codes for ICOMn[3:0] and FCOMn[3:0] on SPI Master**

CONTROL BITS	CODE	ACTION	DESCRIPTION
ICOMn[3:0]	1000	CSBM low	Generates a CSBM Low Signal on SPI Port (GPIO3)
	1001	CSBM high	Generates a CSBM High Signal on SPI Port (GPIO3)
	1111	No Transmit	Releases the SPI Port and Ignores the Rest of the Data
FCOMn[3:0]	X000	CSBM low	Holds CSBM Low at the End of Byte Transmission
	1001	CSBM high	Transitions CSBM High at the End of Byte Transmission

If the bit ICOMn[3] in the COMM register is set to 1 the part becomes an I<sup>2</sup>C master and if the bit is set to 0 the part becomes a SPI master.

Table 16 describes the valid write codes for ICOMn[3:0] and FCOMn[3:0] and their behavior when using the part as an I<sup>2</sup>C master.

Table 17 describes the valid codes for ICOMn[3:0] and FCOMn[3:0] and their behavior when using the part as a SPI master.

Note that only the codes listed in Tables 16 and 17 are valid for ICOMn[3:0] and FCOMn[3:0]. Writing any other code that is not listed in Tables 16 and 17 to ICOMn[3:0] and FCOMn[3:0] may result in unexpected behavior on the I<sup>2</sup>C and SPI ports.

### COMM Commands

Three commands help accomplish I<sup>2</sup>C or SPI communication to the slave device: WRCOMM, STCOMM, RDCOMM

**WRCOMM Command:** This command is used to write data to the COMM register. This command writes 6 bytes of data to the COMM register. The PEC needs to be written

at the end of the data. If the PEC does not match, all data in the COMM register is cleared to 1's when CSB goes high. See the section Bus Protocols for more details on a write command format.

**STCOMM Command:** This command initiates I<sup>2</sup>C/SPI communication on the GPIO ports. The COMM register contains 3 bytes of data to be transmitted to the slave. During this command, the data bytes stored in the COMM register are transmitted to the slave I<sup>2</sup>C or SPI device and the data received from the I<sup>2</sup>C or SPI device is stored in the COMM register. This command uses GPIO4 (SDA) and GPIO5 (SCL) for I<sup>2</sup>C communication or GPIO3 (CSBM), GPIO4 (SDIOM) and GPIO5 (SCKM) for SPI communication.

The STCOMM command is to be followed by 24 clock cycles for each byte of data to be transmitted to the slave device while holding CSB low. For example, to transmit 3 bytes of data to the slave, send STCOMM command and its PEC followed by 72 clock cycles. Pull CSB high at the end of the 72 clock cycles of STCOMM command.

During I<sup>2</sup>C or SPI communication, the data received from the slave device is updated in the COMM register.



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**RDCOMM Command:** The data received from the slave device can be read back from the COMM register using the RDCOMM command. The command reads back 6 bytes of data followed by the PEC. See the section Bus Protocols for more details on a read command format.

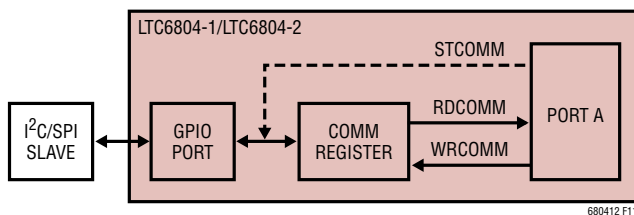
Table 18 describes the possible read back codes for ICOMn[3:0] and FCOMn[3:0] when using the part as an I<sup>2</sup>C master. Dn[7:0] contains the data byte either transmitted by the I<sup>2</sup>C master or received from the I<sup>2</sup>C slave.

In case of the SPI master, the read back codes for ICOMn[3:0] and FCOMn[3:0] are always 0111 and 1111 respectively. Dn[7:0] contains the data byte either transmitted by the SPI master or received from the SPI slave.

**Table 18. Read Codes for ICOMn[3:0] and FCOMn[3:0] on I<sup>2</sup>C Master**

CONTROL BITS	CODE	DESCRIPTION
ICOMn[3:0]	0110	Master Generated a START Signal
	0001	Master Generated a STOP Signal
	0000	Blank, SDA Was Held Low Between Bytes
	0111	Blank, SDA Was Held High Between Bytes
FCOMn[3:0]	0000	Master Generated an ACK Signal
	0111	Slave Generated an ACK Signal
	1111	Slave Generated a NACK Signal
	0001	Slave Generated an ACK Signal, Master Generated a STOP Signal
	1001	Slave Generated a NACK Signal, Master Generated a STOP Signal

Figure 11 illustrates the operation of LTC6804 as an I<sup>2</sup>C or SPI master using the GPIOs.



**Figure 11. LTC6804 I<sup>2</sup>C/SPI Master Using GPIOs**

Any number of bytes can be transmitted to the slave in groups of 3 bytes using these commands. The GPIO ports will not get reset between different STCOMM commands. However, if the wait time between the commands is greater than 2 seconds, the watchdog will timeout and reset the ports to their default values.

To transmit several bytes of data using an I<sup>2</sup>C master, a START signal is only required at the beginning of the entire data stream. A STOP signal is only required at the end of the data stream. All intermediate data groups can use a BLANK code before the data byte and an ACK/NACK signal as appropriate after the data byte. SDA and SCL will not get reset between different STCOMM commands.

To transmit several bytes of data using SPI master, a CSBM low signal is sent at the beginning of the 1st data byte. CSBM can be held low or taken high for intermediate data groups using the appropriate code on FCOMn[3:0]. A CSBM high signal is sent at the end of the last byte of data. CSBM, SDIOM and SCKM will not get reset between different STCOMM commands.

Figure 12 shows the 24 clock cycles following STCOMM command for an I<sup>2</sup>C master in different cases. Note that if ICOMn[3:0] specified a STOP condition, after the STOP signal is sent, the SDA and SCL lines are held high and all data in the rest of the word is ignored. If ICOMn[3:0] is a NO TRANSMIT, both SDA and SCL lines are released, and rest of the data in the word is ignored. This is used when a particular device in the stack does not have to communicate to a slave.

Figure 13 shows the 24 clock cycles following STCOMM command for a SPI master. Similar to the I<sup>2</sup>C master, if ICOMn[3:0] specified a CSBM HIGH or a NO TRANSMIT condition, the CSBM, SCKM and SDIOM lines of the SPI master are released and the rest of the data in the word is ignored.

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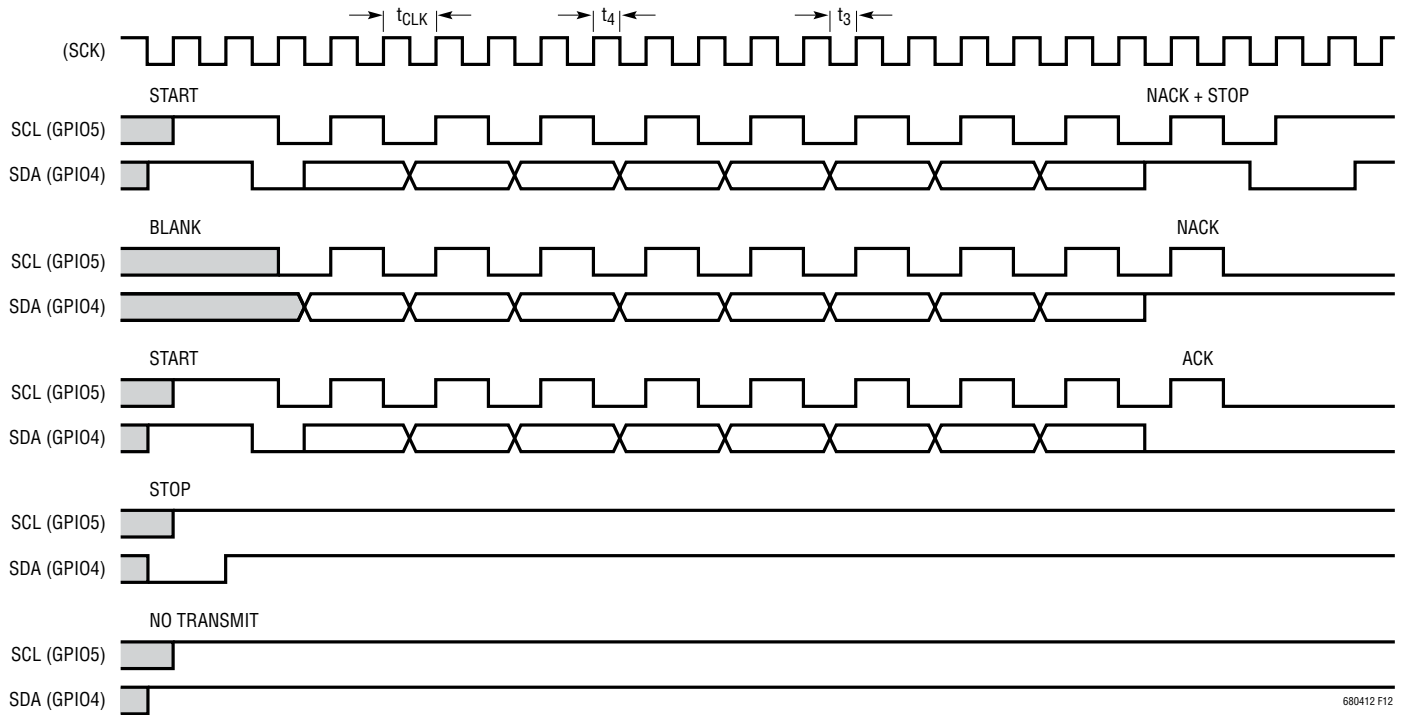


Figure 12. STCOMM Timing Diagram for an I<sup>2</sup>C Master

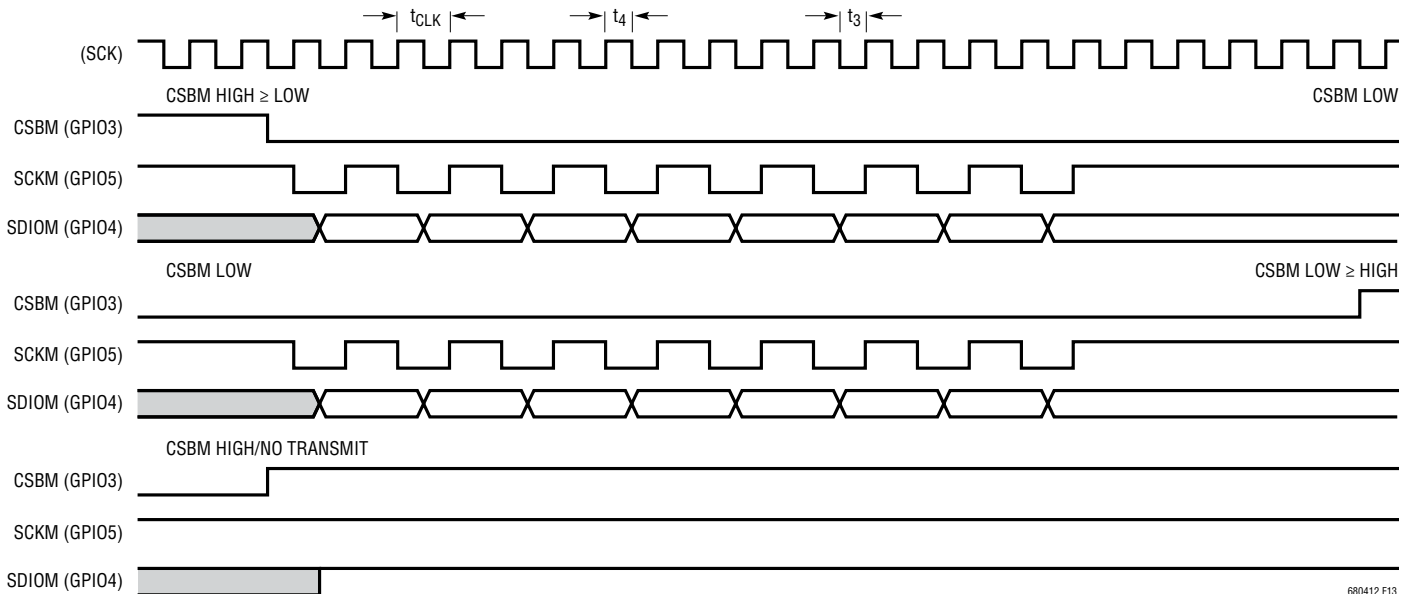


Figure 13. STCOMM Timing Diagram for a SPI Master

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### Timing Specifications of I<sup>2</sup>C and SPI master

The timing of the LTC6804 I<sup>2</sup>C or SPI master will be controlled by the timing of the communication at the LTC6804's primary SPI interface. Table 19 shows the I<sup>2</sup>C master timing relationship to the primary SPI clock. Table 20 shows the SPI master timing specifications.

**Table 19. I<sup>2</sup>C Master Timing**

I <sup>2</sup> C MASTER PARAMETER	TIMING RELATIONSHIP TO PRIMARY SPI INTERFACE	TIMING SPECIFICATIONS AT $t_{CLK} = 1\mu s$
SCL Clock Frequency	$1/(2 \cdot t_{CLK})$	Max 500kHz
$t_{HD}; STA$	$t_3$	Min 200ns
$t_{LOW}$	$t_{CLK}$	Min 1 $\mu s$
$t_{HIGH}$	$t_{CLK}$	Min 1 $\mu s$
$t_{SU}; STA$	$t_{CLK} + t_4^*$	Min 1.03 $\mu s$
$t_{HD}; DAT$	$t_4^*$	Min 30ns
$t_{SU}; DAT$	$t_3$	Min 1 $\mu s$
$t_{SU}; STO$	$t_{CLK} + t_4^*$	Min 1.03 $\mu s$
$t_{BUF}$	$3 \cdot t_{CLK}$	Min 3 $\mu s$

\*Note: When using isoSPI,  $t_4$  is generated internally and is a minimum of 30ns. Also,  $t_3 = t_{CLK} - t_4$ . When using SPI,  $t_3$  and  $t_4$  are the low and high times of the SCK input, each with a specified minimum of 200ns.

### SERIAL INTERFACE OVERVIEW

There are two types of serial ports on the LTC6804, a standard 4-wire serial peripheral interface (SPI) and a 2-wire isolated interface (isoSPI). Pins 41 through 44 are configurable as 2-wire or 4-wire serial port, based on the state of the ISOMD pin.

There are two versions of the LTC6804: the LTC6804-1 and the LTC6804-2. The LTC6804-1 is used in a daisy chain configuration, and the LTC6804-2 is used in an addressable bus configuration. The LTC6804-1 provides a second isoSPI interface using pins 45 through 48. The LTC6804-2 uses pins 45 through 48 to set the address of the device, by tying these pins to  $V^-$  or  $V_{REG}$ .

**Table 20. SPI Master Timing**

SPI MASTER PARAMETER	TIMING RELATIONSHIP TO PRIMARY SPI INTERFACE	TIMING SPECIFICATIONS AT $t_{CLK} = 1\mu s$
SDIOM Valid to SCKM Rising Setup	$t_3$	Min 200ns
SDIOM Valid from SCKM Rising Hold	$t_{CLK} + t_4^*$	Min 1.03 $\mu s$
SCKM Low	$t_{CLK}$	Min 1 $\mu s$
SCKM High	$t_{CLK}$	Min 1 $\mu s$
SCKM Period (SCKM_Low + SCKM_High)	$2 \cdot t_{CLK}$	Min 2 $\mu s$
CSBM Pulse Width	$3 \cdot t_{CLK}$	Min 3 $\mu s$
SCKM Rising to CSBM Rising	$5 \cdot t_{CLK} + t_4^*$	Min 5.03 $\mu s$
CSBM Falling to SCKM Falling	$t_3$	Min 200ns
CSBM Falling to SCKM Rising	$t_{CLK} + t_3$	Min 1.2 $\mu s$
SCKM Falling to SDIOM Valid	Master requires $< t_{CLK}$	

\*Note: When using isoSPI,  $t_4$  is generated internally and is a minimum of 30ns. Also,  $t_3 = t_{CLK} - t_4$ . When using SPI,  $t_3$  and  $t_4$  are the low and high times of the SCK input, each with a specified minimum of 200ns.

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### 4-WIRE SERIAL PERIPHERAL INTERFACE (SPI) PHYSICAL LAYER

#### External Connections

Connecting ISOMD to  $V^-$  configures serial Port A for 4-wire SPI. The SDO pin is an open drain output which requires a pull-up resistor tied to the appropriate supply voltage (Figure 14).

#### Timing

The 4-wire serial port is configured to operate in a SPI system using  $CPHA = 1$  and  $CPOL = 1$ . Consequently, data on SDI must be stable during the rising edge of SCK. The timing is depicted in Figure 15. The maximum data rate is 1Mbps.

### 2-WIRE ISOLATED INTERFACE (isoSPI) PHYSICAL LAYER

The 2-wire interface provides a means to interconnect LTC6804 devices using simple twisted pair cabling. The interface is designed for low packet error rates when the cabling is subjected to high RF fields. Isolation is achieved through an external transformer.

Standard SPI signals are encoded into differential pulses. The strength of the transmission pulse and the threshold level of the receiver are set by two external resistors,  $R_{B1}$  and  $R_{B2}$ . The values of the resistors allow the user to trade off power dissipation for noise immunity.

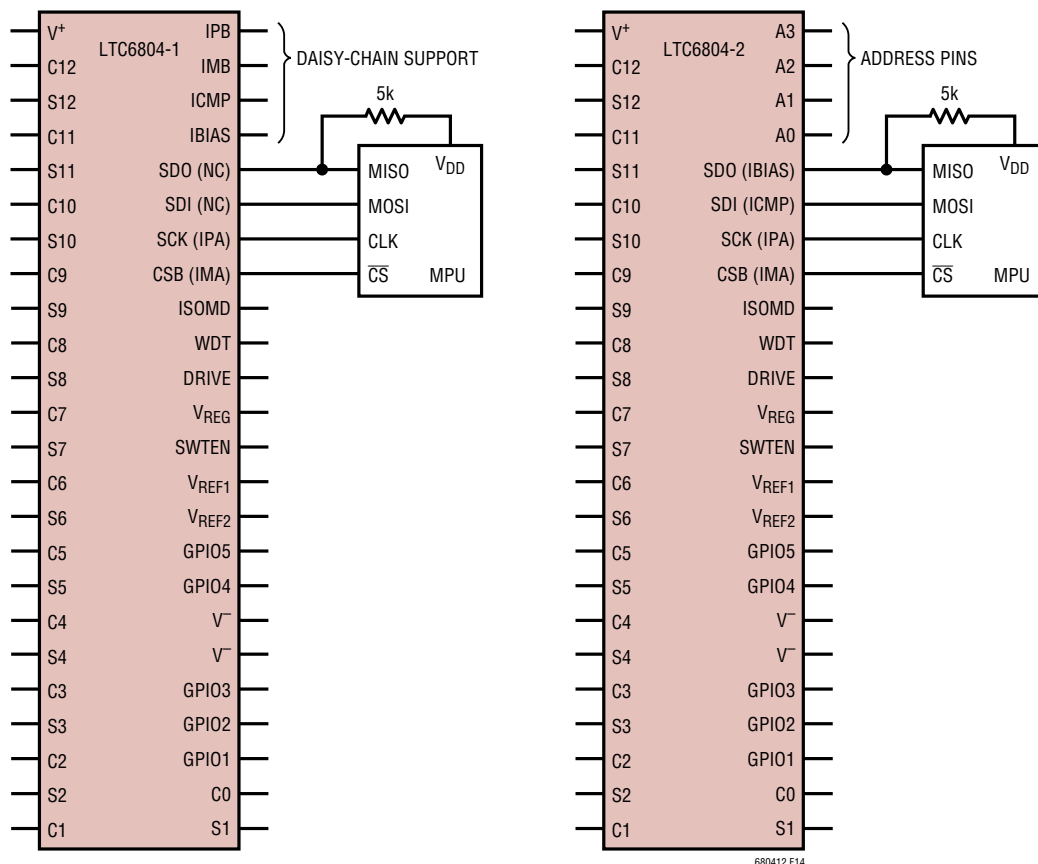


Figure 14. 4-Wire SPI Configuration

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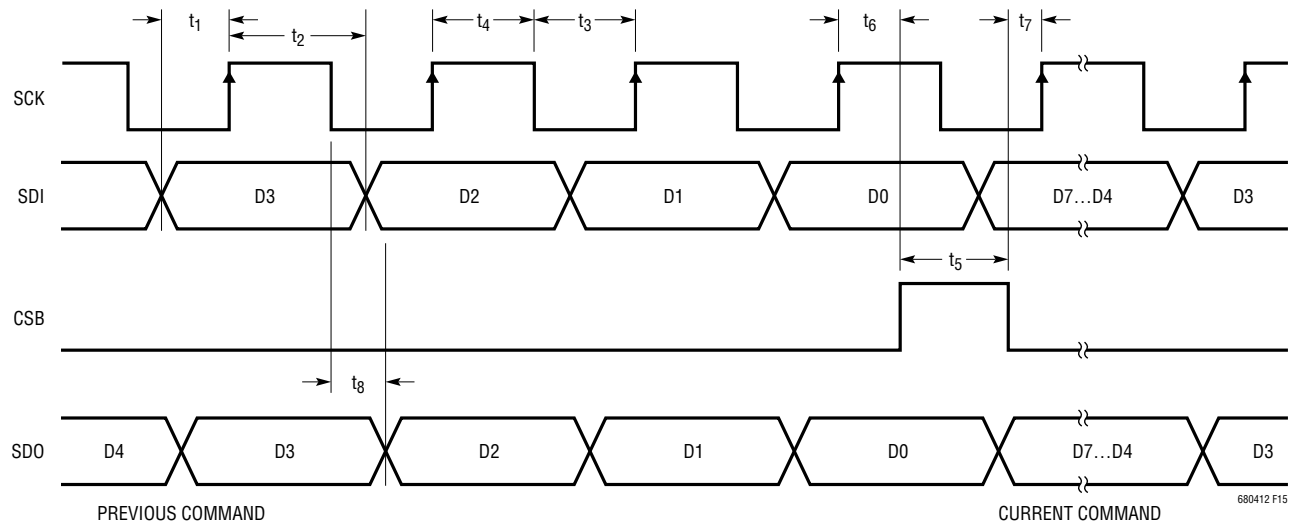


Figure 15. Timing Diagram of 4-Wire Serial Peripheral Interface

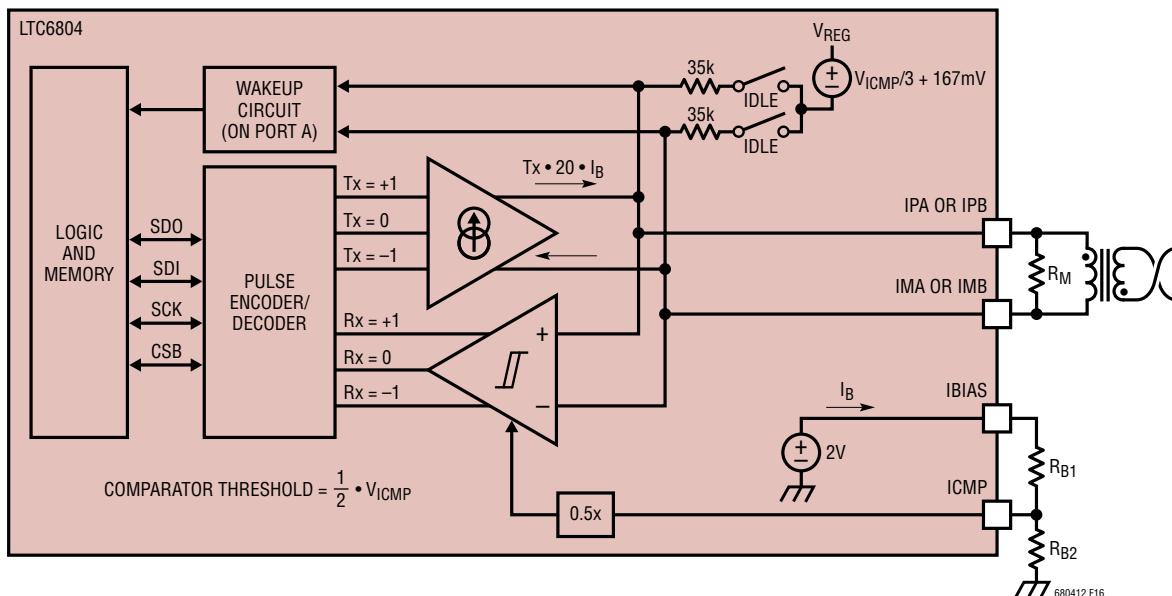


Figure 16. isoSPI Interface

Figure 16 illustrates how the isoSPI circuit operates. A 2V reference drives the IBIAS pin. External resistors  $R_{B1}$  and  $R_{B2}$  create the reference current  $I_B$ . This current sets the drive strength of the transmitter.  $R_{B1}$  and  $R_{B2}$  also form a voltage divider of the 2V reference at the ICMP pin. This sets the threshold voltage of the receiver circuit. Transmitted current pulses are converted into voltage by termination resistor  $R_M$  (in parallel with the characteristic impedance of the cable).

### External Connections

The LTC6804-1 has 2 serial ports which are called Port B and Port A. Port B is always configured as a 2-wire interface (master). The final device in the daisy chain does not use this port, and it should be terminated into  $R_M$ . Port A is either a 2-wire or 4-wire interface (slave), depending on the connection of the ISOMD pin.

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Figure 17a is an example of a robust interconnection of multiple identical PCBs, each containing one LTC6804-1. Note the termination in the final device in the daisy chain. The microprocessor is located on a separate PCB. To achieve 2-wire isolation between the microprocessor PCB and the 1st LTC6804-1 PCB, use the LTC6820 support IC. The LTC6820 is functionally equivalent to the diagram in Figure 16.

The LTC6804-2 has a single serial port (Port A) which can be 2-wire or 4-wire, depending on the state of the ISOMD pin. When configured for 2-wire communications, several devices can be connected in a multi-drop configuration, as shown in Figure 17b. The LTC6820 IC is used to interface the MPU (master) to the LTC6804-2's (slaves).

### Using a Single LTC6804

When only one LTC6804 is needed, the LTC6804-2 is recommended. It does not have isoSPI Port B, so it requires fewer external components and consumes less power, especially when Port A is configured as a 4-wire interface.

However, the LTC6804-1 can be used as a single (non daisy-chained) device if the second isoSPI port (Port B) is properly biased and terminated, as shown in Figure 18c. ICMP should *not* be tied to GND, but can be tied directly to IBIAS. A bias resistance (2k to 20k) is required for IBIAS. Do *not* tie IBIAS directly to  $V_{REG}$  or  $V^-$ . Finally, IPB and IMB should be terminated into a 100 $\Omega$  resistor (not tied to  $V_{REG}$  or  $V^-$ ).

### Selecting Bias Resistors

The adjustable signal amplitude allows the system to trade power consumption for communication robustness, and the adjustable comparator threshold allows the system to account for signal losses.

The isoSPI transmitter drive current and comparator voltage threshold are set by a resistor divider ( $R_{BIAS} = R_{B1} + R_{B2}$ ) between the IBIAS and  $V^-$ . The divided voltage is connected to the ICMP pin which sets the comparator threshold to 1/2 of this voltage ( $V_{ICMP}$ ). When either isoSPI interface is enabled (not IDLE) IBIAS is held at 2V, causing a current  $I_B$  to flow out of the IBIAS pin. The IP and IM pin drive currents are  $20 \cdot I_B$ .

As an example, if divider resistor  $R_{B1}$  is 2.8k and resistor  $R_{B2}$  is 1.21k (so that  $R_{BIAS} = 4k$ ), then:

$$I_B = \frac{2V}{R_{B1} + R_{B2}} = 0.5mA$$

$$I_{DRV} = I_{IP} = I_{IM} = 20 \cdot I_B = 10mA$$

$$V_{ICMP} = 2V \cdot \frac{R_{B2}}{R_{B1} + R_{B2}} = I_B \cdot R_{B2} = 603mV$$

$$V_{TCMP} = 0.5 \cdot V_{ICMP} = 302mV$$

In this example, the pulse drive current  $I_{DRV}$  will be 10mA, and the receiver comparators will detect pulses with IP-IM amplitudes greater than  $\pm 302mV$ .

If the isolation barrier uses 1:1 transformers connected by a twisted pair and terminated with 120 $\Omega$  resistors on each end, then the transmitted differential signal amplitude ( $\pm$ ) will be:

$$V_A = I_{DRV} \cdot \frac{R_M}{2} = 0.6V$$

(This result ignores transformer and cable losses, which may reduce the amplitude).

### isoSPI Pulse Detail

Two LTC6804 devices can communicate by transmitting and receiving differential pulses back and forth through an isolation barrier. The transmitter can output three voltage levels:  $+V_A$ , 0V, and  $-V_A$ . A positive output results from IP sourcing current and IM sinking current across load resistor  $R_M$ . A negative voltage is developed by IP sinking and IM sourcing. When both outputs are off, the load resistance forces the differential output to 0V.

To eliminate the DC signal component and enhance reliability, the isoSPI uses two different pulse lengths. This allows for four types of pulses to be transmitted, as shown in Table 21. A +1 pulse will be transmitted as a positive pulse followed by a negative pulse. A -1 pulse will be transmitted as a negative pulse followed by a positive pulse. The duration of each pulse is defined as  $t_{1/2PW}$ , since each is half of the required symmetric pair. (The total isoSPI pulse duration is  $2 \cdot t_{1/2PW}$ ).

## OPERATION

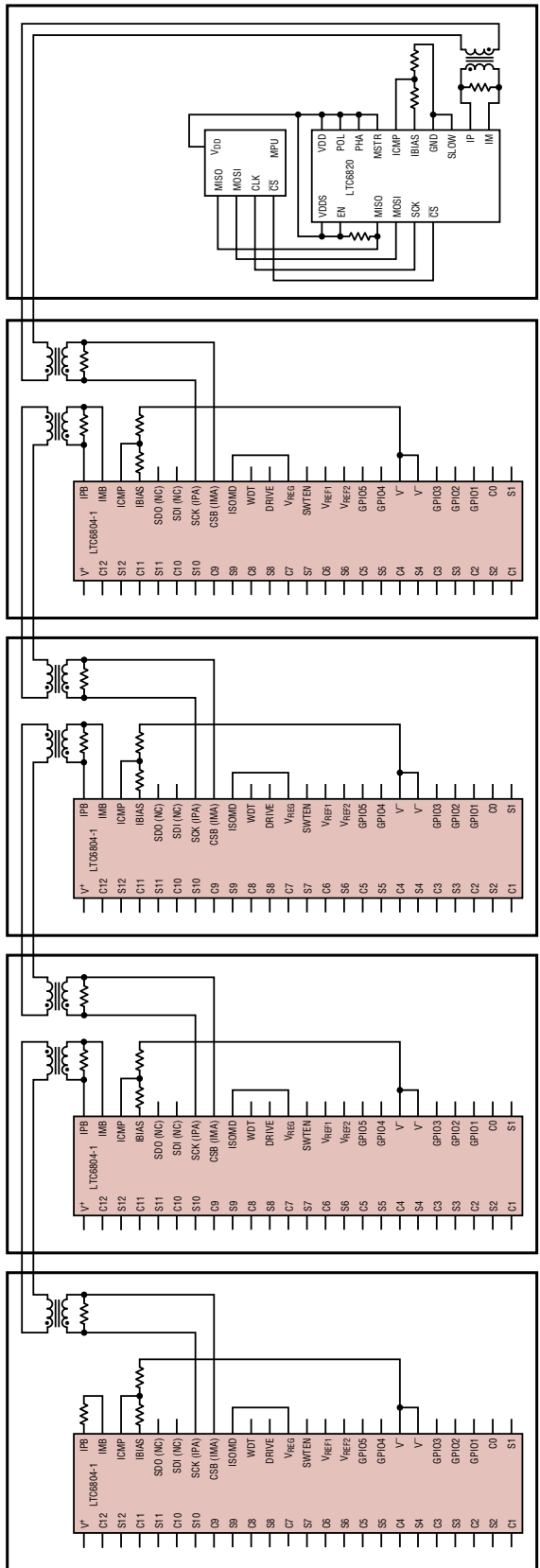


Figure 17a. Transformer-Isolated Daisy-Chain Configuration Using LTC6804-1

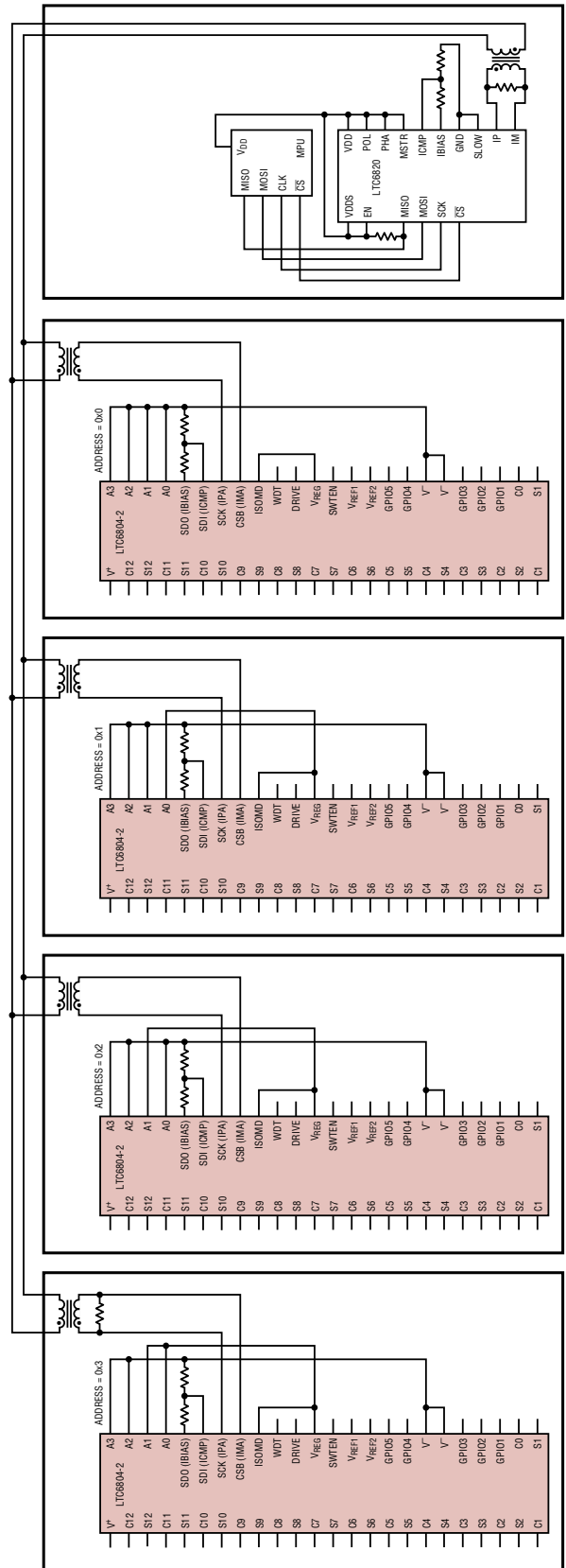


Figure 17b. Multi-Drop Configuration Using LTC6804-2

OPERATION

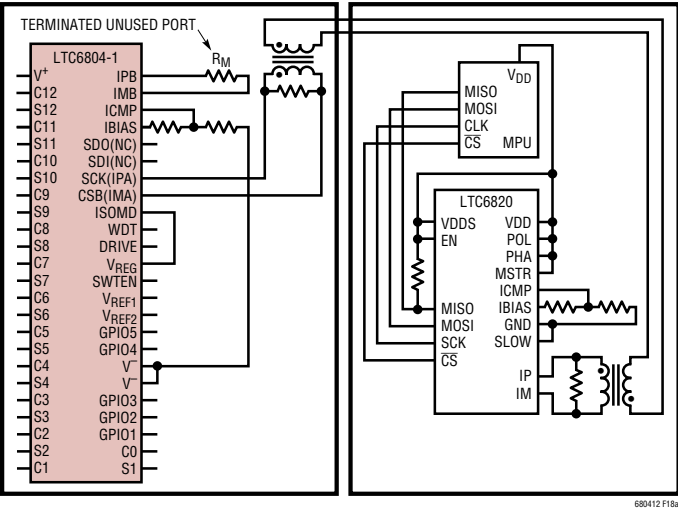


Figure 18a. Single-Device LTC6804-1 Using 2-Wire Port A

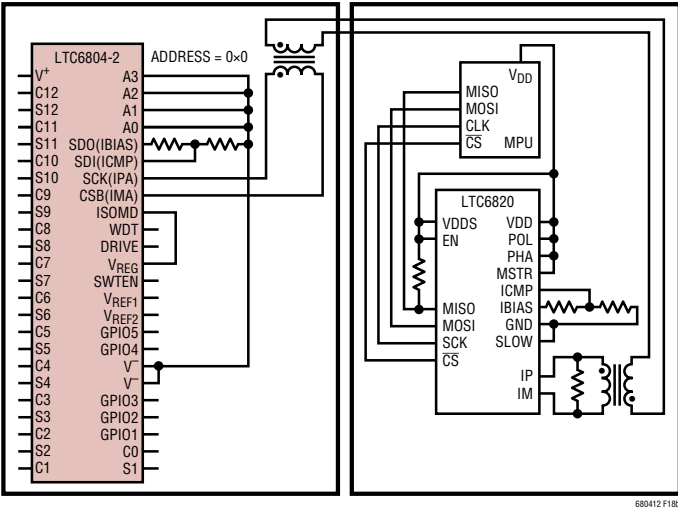


Figure 18b. Single-Device LTC6804-2 Using 2-Wire Port A

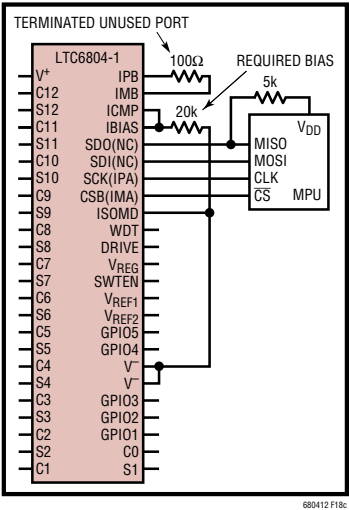


Figure 18c. Single-Device LTC6804-1 Using 4-Wire Port A

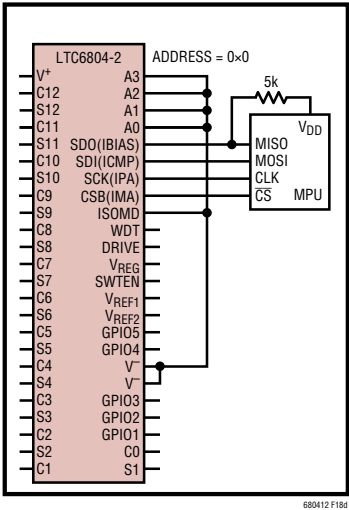


Figure 18d. Single-Device LTC6804-2 Using 4-Wire Port A



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**Table 21. isoSPI Pulse Types**

PULSE TYPE	FIRST LEVEL ( $t_{1/2PW}$ )	SECOND LEVEL ( $t_{1/2PW}$ )	ENDING LEVEL
Long +1	$+V_A$ (150ns)	$-V_A$ (150ns)	0V
Long -1	$-V_A$ (150ns)	$+V_A$ (150ns)	0V
Short +1	$+V_A$ (50ns)	$-V_A$ (50ns)	0V
Short -1	$-V_A$ (50ns)	$+V_A$ (50ns)	0V

A host microcontroller does not have to generate isoSPI pulses to use this 2-wire interface. The first LTC6804 in the system can communicate to the microcontroller using the 4-wire SPI interface on its Port A, then daisy-chain to other LTC6804s using the 2-wire isoSPI interface on its Port B. Alternatively, an LTC6820 can be used to translate the SPI signals into isoSPI pulses.

### LTC6804-1 Operation with Port A Configured for SPI

When the LTC6804-1 is operating with port A as an SPI (ISOMD =  $V^-$ ), the SPI detects one of four communication events: CSB falling, CSB rising, SCK rising with SDI = 0, and SCK rising with SDI = 1. Each event is converted into one of the four pulse types for transmission through the LTC6804-1 daisy chain. Long pulses are used to transmit CSB changes and short pulses are used to transmit data, as explained in Table 22.

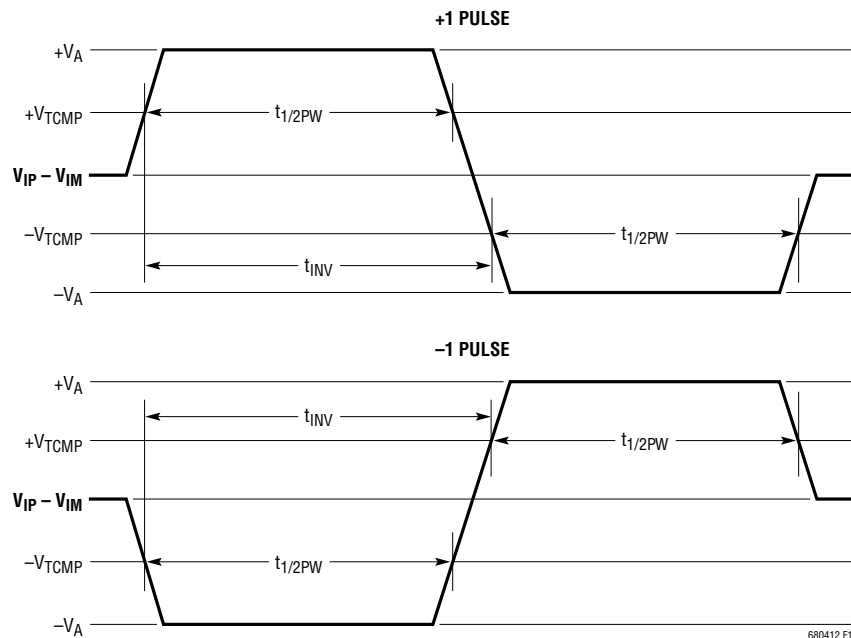
**Table 22. LTC6804-1 Port B (Master) isoSPI Port Function**

COMMUNICATION EVENT (PORT A SPI)	TRANSMITTED PULSE (PORT B isoSPI)
CSB Rising	Long +1
CSB Falling	Long -1
SCK Rising Edge, SDI = 1	Short +1
SCK Rising Edge, SDI = 0	Short -1

On the other side of the isolation barrier (i.e. at the other end of the cable), the 2nd LTC6804 will have ISOMD =  $V_{REG}$ . Its Port A operates as a slave isoSPI interface. It receives each transmitted pulse and reconstructs the SPI signals internally, as shown in Table 23. In addition, during a READ command this port may transmit return data pulses.

**Table 23. LTC6804-1 Port A (Slave) isoSPI Port Function**

RECEIVED PULSE (PORT A isoSPI)	INTERNAL SPI PORT ACTION	RETURN PULSE
Long +1	Drive CSB High	None
Long -1	Drive CSB Low	
Short +1	1. Set SDI = 1 2. Pulse SCK	Short -1 Pulse if Reading a 0 bit
Short -1	1. Set SDI = 0 2. Pulse SCK	(No Return Pulse if Not in READ Mode or if Reading a 1 bit)



**Figure 19. isoSPI Pulse Detail**

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The lower isoSPI port (Port A) never transmits long (CSB) pulses. Furthermore, a slave isoSPI port will only transmit short  $-1$  pulses, never a  $+1$  pulse. The master port recognizes a null response as a logic 1. This allows for multiple slave devices on a single cable without risk of collisions (Multidrop).

Figure 20 shows the isoSPI timing diagram for a READ command to daisy-chained LTC6804-1 parts. The ISOMD pin is tied to  $V^-$  on the bottom part so its Port A is configured as a SPI port (CSB, SCK, SDI and SDO). The isoSPI signals of three stacked devices are shown, labeled with the port (A or B) and part number. Note that ISO B1 and ISO A2 is actually the same signal, but shown on each end of the transmission cable that connects parts 1 and 2. Likewise, ISO B2 and ISO A3 is the same signal, but with the cable delay shown between parts 2 and 3.

Bits  $W_n$ - $W_0$  refers to the 16-bit command code and the 16-bit PEC of a READ command. At the end of bit  $W_0$  the 3 parts decode the READ command and begin shifting out data which is valid on the next rising edge of clock SCK. Bits  $X_n$ - $X_0$  refer to the data shifted out by Part 1. Bits  $Y_n$ - $Y_0$  refer to the data shifted out by Part 2 and bits  $Z_n$ - $Z_0$  refer to the data shifted out by Part 3. All this data is read back from the SDO port on Part 1 in a daisy-chained fashion.

### Waking Up the Serial Interface

The serial ports (SPI or isoSPI) will enter the low power IDLE state if there is no activity on Port A for a time of  $t_{IDLE}$ . The WAKEUP circuit monitors activity on pins 41 and 42.

If ISOMD =  $V^-$ , Port A is in SPI mode. Activity on the CSB or SCK pin will wake up the SPI interface. If ISOMD =  $V_{REG}$ ,

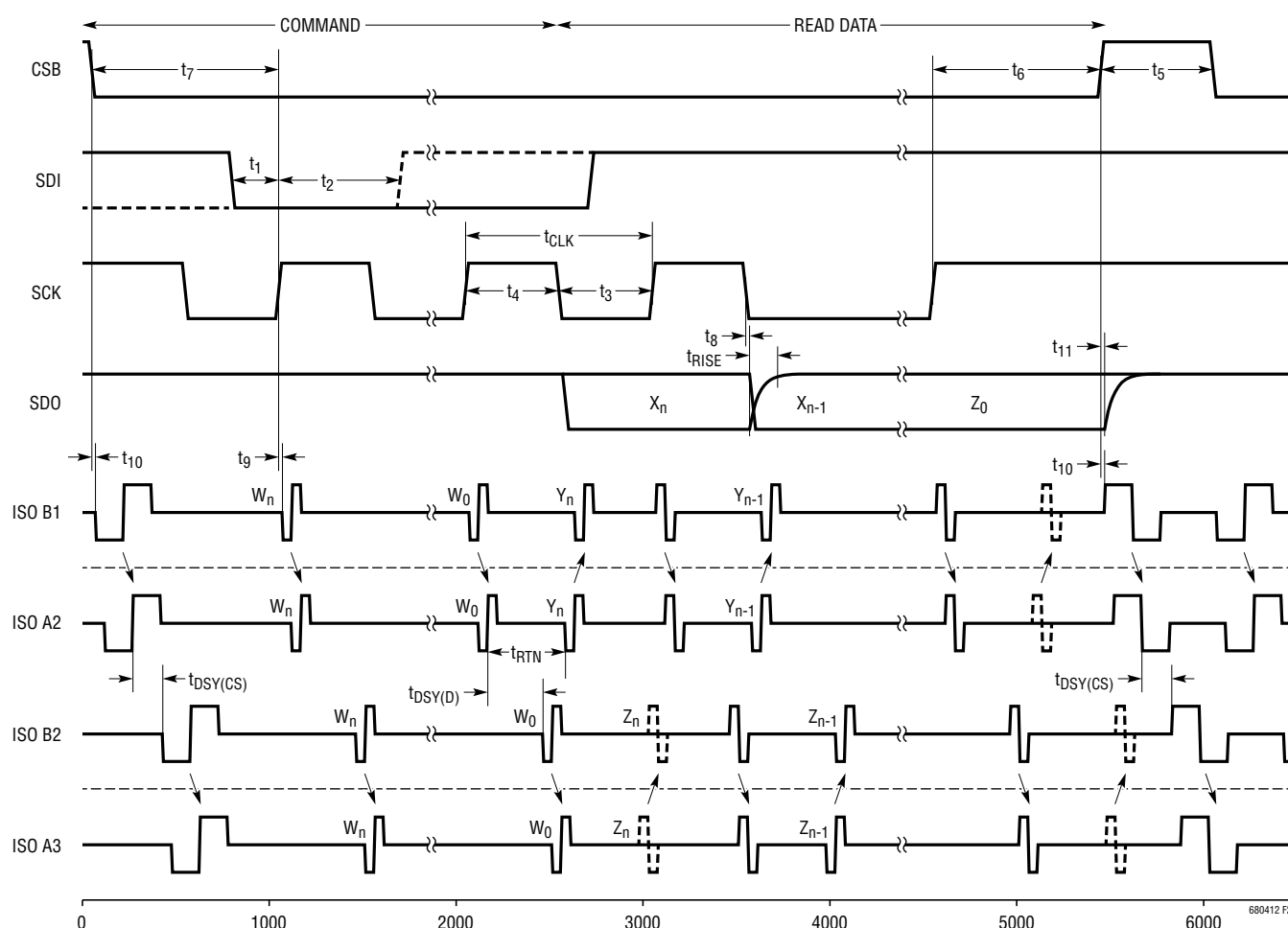


Figure 20. isoSPI Timing Diagram

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Port A is in isoSPI mode. Differential activity on IPA-IMB wakes up the isoSPI interface. The LTC6804 will be ready to communicate when the isoSPI state changes to READY within  $t_{WAKE}$  or  $t_{READY}$ , depending on the Core state (see Figure 1 and state descriptions for details.)

Figure 21 illustrates the timing and the functionally equivalent circuit. Common mode signals will not wake up the serial interface. The interface is designed to wake up after receiving a large signal single-ended pulse, or a low-amplitude symmetric pulse. The differential signal  $|SCK(IPA) - CSB(IMA)|$ , must be at least  $V_{WAKE} = 200mV$  for a minimum duration of  $t_{DWELL} = 240ns$  to qualify as a wake up signal that powers up the serial interface.

### Waking a Daisy Chain — Method 1

The LTC6804-1 sends a Long +1 pulse on Port B after it is ready to communicate. In a daisy-chained configuration, this pulse wakes up the next device in the stack which will, in turn, wake up the next device. If there are 'N' devices in the stack, all the devices are powered up within the time  $N \cdot t_{WAKE}$  or  $N \cdot t_{READY}$ , depending on the Core State. For large stacks, the time  $N \cdot t_{WAKE}$  may be equal to or larger than  $t_{IDLE}$ . In this case, after waiting longer than the time of  $N \cdot t_{WAKE}$ , the host may send another dummy byte and wait for the time  $N \cdot t_{READY}$ , in order to ensure that all devices are in the READY state.

Method 1 can be used when all devices on the daisy chain are in the IDLE state. This guarantees that they propagate the wake-up signal up the daisy chain. However, this method will fail to wake up all devices when a device in the middle of the chain is in the READY state instead of IDLE. When this happens, the device in READY state will not propagate the wake-up pulse, so the devices above it will remain IDLE. This situation can occur when attempting to wake up the daisy chain after only  $t_{IDLE}$  of idle time (some devices may be IDLE, some may not).

### Waking a Daisy Chain — Method 2

A more robust wake-up method does not rely on the built-in wake-up pulse, but manually sends isoSPI traffic for enough time to wake the entire daisy chain. At minimum, a pair of long isoSPI pulses (–1 and +1) is needed for each device, separated by more than  $t_{READY}$  or  $t_{WAKE}$  (if the core state is STANDBY or SLEEP, respectively), but less than  $t_{IDLE}$ . This allows each device to wake up and propagate the next pulse to the following device. This method works even if some devices in the chain are not in the IDLE state. In practice, implementing method 2 requires toggling the CSB pin (of the LTC6820, or bottom LTC6804-1 with ISOMD = 0) to generate the long isoSPI pulses. Alternatively, dummy commands (such as RDCFG) can be executed to generate the long isoSPI pulses.

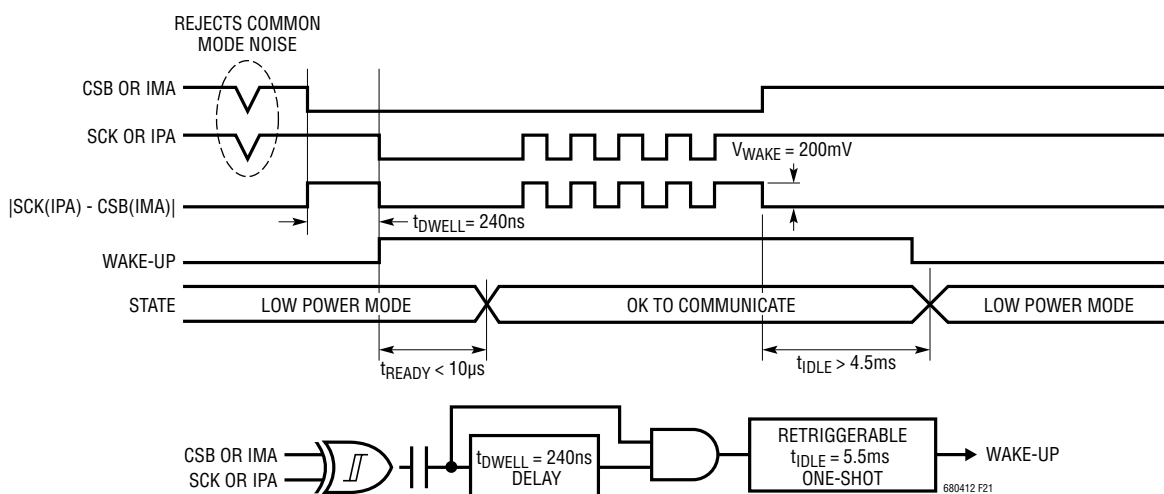


Figure 21. Wake-Up Detection and IDLE Timer

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### DATA LINK LAYER

All Data transfers on LTC6804 occur in byte groups. Every byte consists of 8 bits. Bytes are transferred with the most significant bit (MSB) first. CSB must remain low for the entire duration of a command sequence, including between a command byte and subsequent data. On a write command, data is latched in on the rising edge of CSB.

### NETWORK LAYER

#### Packet Error Code

The packet error code (PEC) is a 15-bit cyclic redundancy check (CRC) value calculated for all of the bits in a register group in the order they are passed, using the initial PEC seed value of 000000000010000 and the following characteristic polynomial:  $x^{15} + x^{14} + x^{10} + x^8 + x^7 + x^4 + x^3 + 1$ . To calculate the 15-bit PEC value, a simple procedure can be established:

1. Initialize the PEC to 000000000010000 (PEC is a 15-bit register group)
2. For each bit DIN coming into the PEC register group, set
  - $IN0 = DIN \text{ XOR } PEC[14]$
  - $IN3 = IN0 \text{ XOR } PEC[2]$
  - $IN4 = IN0 \text{ XOR } PEC[3]$
  - $IN7 = IN0 \text{ XOR } PEC[6]$
  - $IN8 = IN0 \text{ XOR } PEC[7]$
  - $IN10 = IN0 \text{ XOR } PEC[9]$
  - $IN14 = IN0 \text{ XOR } PEC[13]$

3. Update the 15-bit PEC as follows

$$\begin{aligned} PEC[14] &= IN14, \\ PEC[13] &= PEC[12], \\ PEC[12] &= PEC[11], \\ PEC[11] &= PEC[10], \\ PEC[10] &= IN10, \\ PEC[9] &= PEC[8], \\ PEC[8] &= IN8, \\ PEC[7] &= IN7, \\ PEC[6] &= PEC[5], \\ PEC[5] &= PEC[4], \\ PEC[4] &= IN4, \\ PEC[3] &= IN3, \\ PEC[2] &= PEC[1], \\ PEC[1] &= PEC[0], \\ PEC[0] &= IN0 \end{aligned}$$

4. Go back to step 2 until all the data is shifted. The final PEC (16 bits) is the 15-bit value in the PEC register with a 0 bit appended to its LSB

Figure 22 illustrates the algorithm described above. An example to calculate the PEC for a 16-bit word (0x0001) is listed in Table 24. The PEC for 0x0001 is computed as 0x3D6E after stuffing a 0 bit at the LSB. For longer data streams, the PEC is valid at the end of the last bit of data sent to the PEC register.

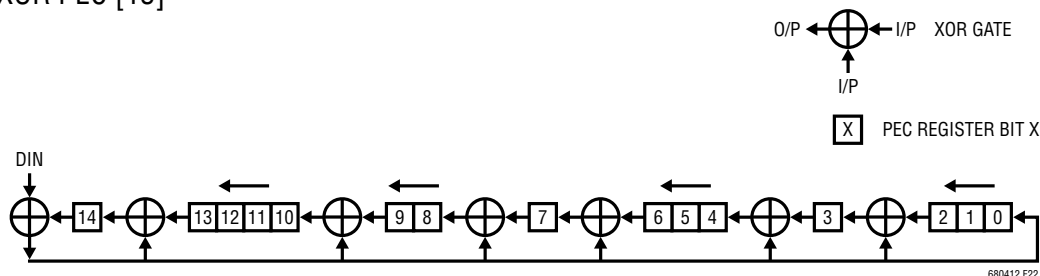


Figure 22. 15-Bit PEC Computation Circuit

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LTC6804 calculates PEC for any command or data received and compares it with the PEC following the command or data. The command or data is regarded as valid only if the PEC matches. LTC6804 also attaches the calculated PEC at the end of the data it shifts out. Table 25 shows the format of PEC while writing to or reading from LTC6804.

While writing any command to LTC6804, the command bytes CMD0 and CMD1 (See Table 32 and Table 33) and the PEC bytes PEC0 and PEC1 are sent on Port A in the following order:

CMD0, CMD1, PEC0, PEC1

After a broadcast write command to daisy-chained LTC6804-1 devices, data is sent to each device followed by the PEC. For example, when writing the configuration

register group to two daisy-chained devices (primary device P, stacked device S), the data will be sent to the primary device on Port A in the following order:

CFGR0(S), ..., CFGR5(S), PEC0(S), PEC1(S), CFGR0(P), ..., CFGR5(P), PEC0(P), PEC1(P)

After a read command for daisy-chained devices, each device shifts out its data and the PEC that it computed for its data on Port A followed by the data received on Port B. For example, when reading status register group B from two daisy-chained devices (primary device P, stacked device S), the primary device sends out data on port A in the following order:

STBR0(P), ..., STBR5(P), PEC0(P), PEC1(P), STBR0(S), ..., STBR5(S), PEC0(S), PEC1(S)

**Table 24. PEC Calculation for 0x0001**

PEC[14]	0	0	0	0	0	0	0	0	0	0	1	1	1	1	1	0	0	<b>0</b>
PEC[13]	0	0	0	0	0	0	0	0	0	1	0	0	0	0	1	1	0	<b>0</b>
PEC[12]	0	0	0	0	0	0	0	0	1	0	0	0	0	1	1	0	1	<b>1</b>
PEC[11]	0	0	0	0	0	0	0	1	0	0	0	0	1	1	0	1	1	<b>1</b>
PEC[10]	0	0	0	0	0	0	1	0	0	0	0	1	1	0	1	1	1	<b>1</b>
PEC[9]	0	0	0	0	0	1	0	0	0	0	0	0	1	0	0	0	1	<b>1</b>
PEC[8]	0	0	0	0	1	0	0	0	0	0	0	1	0	0	0	1	0	<b>0</b>
PEC[7]	0	0	0	1	0	0	0	0	0	0	0	1	1	1	0	1	1	<b>1</b>
PEC[6]	0	0	1	0	0	0	0	0	0	0	0	0	0	1	0	0	0	<b>0</b>
PEC[5]	0	1	0	0	0	0	0	0	0	0	0	0	1	0	0	0	1	<b>1</b>
PEC[4]	1	0	0	0	0	0	0	0	0	0	0	1	0	0	0	1	1	<b>1</b>
PEC[3]	0	0	0	0	0	0	0	0	0	0	0	1	1	1	0	0	0	<b>0</b>
PEC[2]	0	0	0	0	0	0	0	0	0	0	0	0	0	1	1	1	1	<b>1</b>
PEC[1]	0	0	0	0	0	0	0	0	0	0	0	0	1	1	1	1	1	<b>1</b>
PEC[0]	0	0	0	0	0	0	0	0	0	0	0	1	1	1	1	1	1	<b>1</b>
IN14	0	0	0	0	0	0	0	0	0	1	1	1	1	1	0	0		<b>0</b>
IN10	0	0	0	0	0	1	0	0	0	0	1	1	0	1	1	1		<b>PEC Word</b>
IN8	0	0	0	1	0	0	0	0	0	0	1	0	0	0	1	0		
IN7	0	0	1	0	0	0	0	0	0	0	1	1	1	0	1	1		
IN4	0	0	0	0	0	0	0	0	0	0	1	0	0	0	1	1		
IN3	0	0	0	0	0	0	0	0	0	0	1	1	1	0	0	0		
IN0	0	0	0	0	0	0	0	0	0	0	1	1	1	1	1	1		
DIN	0	0	0	0	0	0	0	0	0	0	0	0	0	0	0	1		
Clock Cycle	0	1	2	3	4	5	6	7	8	9	10	11	12	13	14	15	16	

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**Table 25. Write/Read PEC Format**

NAME	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
PEC0	RD/WR	PEC[14]	PEC[13]	PEC[12]	PEC[11]	PEC[10]	PEC[9]	PEC[8]	PEC[7]
PEC1	RD/WR	PEC[6]	PEC[5]	PEC[4]	PEC[3]	PEC[2]	PEC[1]	PEC[0]	0

**Broadcast vs Address Commands**

CONFIGURATION		TYPE OF COMMAND		
DEVICE	INTERFACE	READ	WRITE	POLL
LTC6804-2 (Address/Parallel)	SPI	Address-Only	Address or Broadcast	Address or Broadcast
	isoSPI			Address-Only <sup>†</sup>
LTC6804-1 (Daisy-Chain)	SPI or isoSPI	Broadcast-Only		N/A

<sup>†</sup>The LTC6804-2 will not return data pulses when using broadcast commands in isoSPI mode. Therefore, ADC commands will execute, but polling will not work.

**Address Commands (LTC6804-2 Only)**

An address command is one in which only the addressed device on the bus responds. Address commands are used only with LTC6804-2 parts. All commands are compatible with addressing. See Bus Protocols for Address command format.

**Broadcast Commands (LTC6804-1 or LTC6804-2)**

A broadcast command is one to which all devices on the bus will respond, regardless of device address. This command format can be used with LTC6804-1 and LTC6804-2 parts. See Bus Protocols for Broadcast command format. With broadcast commands all devices can be sent commands simultaneously.

In parallel (LTC6804-2) configurations, broadcast commands are useful for initiating ADC conversions or for sending write commands when all parts are being written with the same data. The polling function (automatic at the end of ADC commands, or manual using the PLADC command) can also be used with broadcast commands, but only with parallel SPI interfaces. Polling is not compatible with parallel isoSPI. Likewise, broadcast read commands should not be used in a parallel configuration (either SPI or isoSPI).

Daisy-chained (LTC6804-1) configurations support broadcast commands only, because they have no addressing. All devices in the chain receive the command bytes simultaneously. For example, to initiate ADC conversions in a stack of devices, a single ADCV command is sent, and all devices will start conversions at the same time. For read and write commands, a single command is sent, and then the stacked devices effectively turn into a cascaded shift register, in which data is shifted through each device to the next device in the stack. See the Serial Programming Examples section.

**Polling Methods**

The simplest method to determine ADC completion is for the controller to start an ADC conversion and wait for the specified conversion time to pass before reading the results. Polling is not supported with daisy-chain communication (LTC6804-1).

In parallel configurations that communicate in SPI mode (ISOMD pin tied low), there are two methods of polling. The first method is to hold CSB low after an ADC conversion command is sent. After entering a conversion command, the SDO line is driven low when the device is busy performing conversions (Figure 23). SDO is pulled high when the device completes conversions. However, the SDO will also go back high when CSB goes high even if the device has not completed the conversion. An addressed device drives the SDO line based on its status alone. A problem with this method is that the controller is not free to do other serial communication while waiting for ADC conversions to complete.

The next method overcomes this limitation. The controller can send an ADC start command, perform other tasks, and then send a poll ADC converter status (PLADC) command to determine the status of the ADC conversions (Figure 24). After entering the PLADC command, SDO will go low if the device is busy performing conversions. SDO is pulled high at the end of conversions. However, the SDO will also

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go high when CSB goes high even if the device has not completed the conversion. See Programming Examples on how to use the PLADC command with devices in parallel configuration.

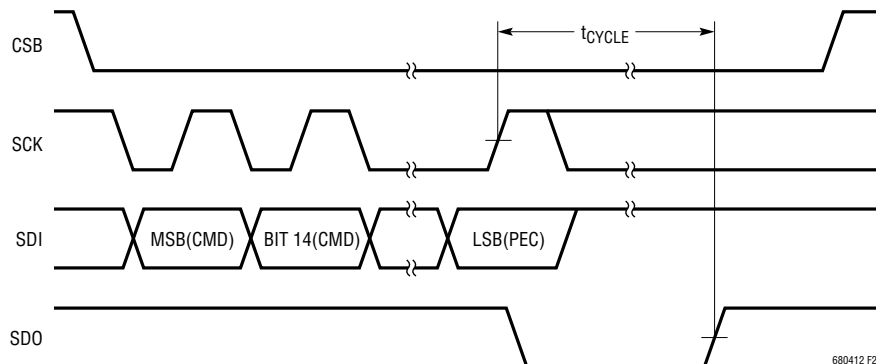
In parallel configurations that communicate in isoSPI mode, the low side port transmits a data pulse only in response to a master isoSPI pulse received by it. So, after entering an address command in either method of polling described above, isoSPI data pulses are sent to the part to update the conversion status. These pulses can be sent using LTC6820 by simply clocking its SCK pin. In response to this pulse, the LTC6804-2 returns an isoSPI pulse if it is still busy performing conversions and does not return a pulse if it has completed conversions. If a CSB high isoSPI pulse is sent to the LTC6804-2, it exits the polling command. Note that broadcast poll commands are not compatible with parallel isoSPI.

### Bus Protocols

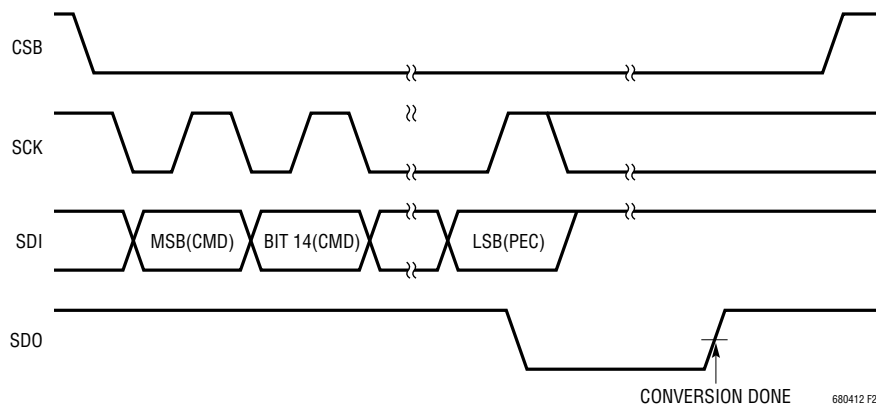
**Protocol Format:** The protocol formats for both broadcast and address commands are depicted in Table 27 through Table 31. Table 26 is the key for reading the protocol diagrams.

**Table 26. Protocol Key**

CMD0	First Command Byte (See Tables 32 and 33)
CMD1	Second Command Byte (See Tables 32 and 33)
PEC0	First PEC Byte (See Table 25)
PEC1	Second PEC Byte (See Table 25)
$n$	Number of Bytes
...	Continuation of Protocol
	Master to Slave
	Slave to Master



**Figure 23. SDO Polling After an ADC Conversion Command**



**Figure 24. SDO Polling Using PLADC Command**



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**Command Format:** The formats for the broadcast and address commands are shown in Table 32 and Table 33 respectively. The 11-bit command code CC[10:0] is the same for a broadcast or an address command. A list of all the command codes is shown in Table 34. A broadcast command has a value 0 for CMD0[7] through CMD0[3]. An address command has a value 1 for CMD0[7] followed by the 4-bit address of the device (a3, a2, a1, a0) in bits CMD0[6:3]. An addressed device will respond to an address

command only if the physical address of the device on pins A3 to A0 match the address specified in the address command. The PEC for broadcast and address commands must be computed on the entire 16-bit command (CMD0 and CMD1).

### Commands

Table 34 lists all the commands and its options for both LTC6804-1 and LTC6804-2

**Table 27. Broadcast/Address Poll Command**

8	8	8	8	
CMD0	CMD1	PEC0	PEC1	Poll Data

**Table 28. Broadcast Write Command (LTC6804-1)**

8	8	8	8	8		8	8	8	8		8
CMD0	CMD1	PEC0	PEC1	Data Byte Low	...	Data Byte High	PEC0	PEC1	Shift Byte 1	...	Shift Byte <i>n</i>

**Table 29. Broadcast/Address Write Command (LTC6804-2)**

8	8	8	8	8		8	8	8
CMD0	CMD1	PEC0	PEC1	Data Byte Low	...	Data Byte High	PEC0	PEC1

**Table 30. Broadcast Read Command (LTC6804-1)**

8	8	8	8	8		8	8	8	8		8
CMD0	CMD1	PEC0	PEC1	Data Byte Low	...	Data Byte High	PEC0	PEC1	Shift Byte 1	...	Shift Byte <i>n</i>

**Table 31. Address Read Command (LTC6804-2)**

8	8	8	8	8		8	8	8
CMD0	CMD1	PEC0	PEC1	Data Byte Low	...	Data Byte High	PEC0	PEC1

**Table 32. Broadcast Command Format**

NAME	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CMD0	WR	0	0	0	0	0	CC[10]	CC[9]	CC[8]
CMD1	WR	CC[7]	CC[6]	CC[5]	CC[4]	CC[3]	CC[2]	CC[1]	CC[0]

**Table 33. Address Command Format**

NAME	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CMD0	WR	1	a3*	a2*	a1*	a0*	CC[10]	CC[9]	CC[8]
CMD1	WR	CC[7]	CC[6]	CC[5]	CC[4]	CC[3]	CC[2]	CC[1]	CC[0]

\*ax is Address Bit x

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**Table 34. Command Codes**

COMMAND DESCRIPTION	NAME	CC[10:0] - COMMAND CODE										
		10	9	8	7	6	5	4	3	2	1	0
Write Configuration Register Group	WRCFG	0	0	0	0	0	0	0	0	0	0	1
Read Configuration Register Group	RDCFG	0	0	0	0	0	0	0	0	0	1	0
Read Cell Voltage Register Group A	RDCVA	0	0	0	0	0	0	0	0	1	0	0
Read Cell Voltage Register Group B	RDCVB	0	0	0	0	0	0	0	0	1	1	0
Read Cell Voltage Register Group C	RDCVC	0	0	0	0	0	0	0	1	0	0	0
Read Cell Voltage Register Group D	RDCVD	0	0	0	0	0	0	0	1	0	1	0
Read Auxiliary Register Group A	RDAUXA	0	0	0	0	0	0	0	1	1	0	0
Read Auxiliary Register Group B	RDAUXB	0	0	0	0	0	0	0	1	1	1	0
Read Status Register Group A	RDSTATA	0	0	0	0	0	0	1	0	0	0	0
Read Status Register Group B	RDSTATB	0	0	0	0	0	0	1	0	0	1	0
Start Cell Voltage ADC Conversion and Poll Status	ADCV	0	1	MD[1]	MD[0]	1	1	DCP	0	CH[2]	CH[1]	CH[0]
Start Open Wire ADC Conversion and Poll Status	ADOW	0	1	MD[1]	MD[0]	PUP	1	DCP	1	CH[2]	CH[1]	CH[0]
Start Self-Test Cell Voltage Conversion and Poll Status	CVST	0	1	MD[1]	MD[0]	ST[1]	ST[0]	0	0	1	1	1
Start GPIOs ADC Conversion and Poll Status	ADAX	1	0	MD[1]	MD[0]	1	1	0	0	CHG [2]	CHG [1]	CHG [0]
Start Self-Test GPIOs Conversion and Poll Status	AXST	1	0	MD[1]	MD[0]	ST[1]	ST[0]	0	0	1	1	1
Start Status group ADC Conversion and Poll Status	ADSTAT	1	0	MD[1]	MD[0]	1	1	0	1	CHST [2]	CHST [1]	CHST [0]
Start Self-Test Status group Conversion and Poll Status	STATST	1	0	MD[1]	MD[0]	ST[1]	ST[0]	0	1	1	1	1
Start Combined Cell Voltage and GPIO1, GPIO2 Conversion and Poll Status	ADCVAX	1	0	MD[1]	MD[0]	1	1	DCP	1	1	1	1
Clear Cell Voltage Register Group	CLRCELL	1	1	1	0	0	0	1	0	0	0	1
Clear Auxiliary Register Group	CLRAUX	1	1	1	0	0	0	1	0	0	1	0
Clear Status Register Group	CLRSTAT	1	1	1	0	0	0	1	0	0	1	1
Poll ADC Conversion Status	PLADC	1	1	1	0	0	0	1	0	1	0	0
Diagnose MUX and Poll Status	DIAGN	1	1	1	0	0	0	1	0	1	0	1
Write COMM Register Group	WRCOMM	1	1	1	0	0	1	0	0	0	0	1
Read COMM Register Group	RDCOMM	1	1	1	0	0	1	0	0	0	1	0
Start I <sup>2</sup> C/SPI Communication	STCOMM	1	1	1	0	0	1	0	0	0	1	1

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Table 35. Command Bit Descriptions

NAME	DESCRIPTION	VALUES								
MD[1:0]	ADC Mode	MD	ADCOPT(CFGR0[0]) = 0				ADCOPT (CFGR0[0]) = 1			
		01	27kHz Mode (Fast)				14kHz Mode			
		10	7kHz Mode (Normal)				3kHz Mode			
		11	26Hz Mode (Filtered)				2kHz Mode			
DCP	Discharge Permitted	DCP								
		0	Discharge Not Permitted							
		1	Discharge Permitted							
CH[2:0]	Cell Selection for ADC Conversion			Total Conversion Time in the 6 ADC Modes						
		CH		27kHz	14kHz	7kHz	3kHz	2kHz	26Hz	
		000	All Cells	1.1ms	1.3ms	2.3ms	3.0ms	4.4ms	201ms	
		001	Cell 1 and Cell 7	201μs	230μs	405μs	501μs	754μs	34ms	
		010	Cell 2 and Cell 8							
		011	Cell 3 and Cell 9							
		100	Cell 4 and Cell 10							
		101	Cell 5 and Cell 11							
		110	Cell 6 and Cell 12							
PUP	Pull-Up/Pull-Down Current for Open-Wire Conversions	PUP								
		0	Pull-Down Current							
		1	Pull-Up Current							
ST[1:0]	Self-Test Mode Selection			Self-Test Conversion Result						
		ST		27kHz	14kHz	7kHz	3kHz	2kHz	26Hz	
		01	Self Test 1	0x9565	0x9553	0x9555	0x9555	0x9555	0x9555	
		10	Self test 2	0x6A9A	0x6AAC	0x6AAA	0x6AAA	0x6AAA	0x6AAA	
CHG[2:0]	GPIO Selection for ADC Conversion			Total Conversion Time in the 6 ADC Modes						
		CHG		27kHz	14kHz	7kHz	3kHz	2kHz	26Hz	
		000	GPIO 1-5, 2nd Ref	1.1ms	1.3ms	2.3ms	3.0ms	4.4ms	201ms	
		001	GPIO 1	201μs	230μs	405μs	501μs	754μs	34ms	
		010	GPIO 2							
		011	GPIO 3							
		100	GPIO 4							
		101	GPIO 5							
110	2nd Reference									
CHST[2:0]*	Status Group Selection			Total Conversion Time in the 6 ADC Modes						
		CHST		27kHz	14kHz	7kHz	3kHz	2kHz	26Hz	
		000	SOC, ITMP, VA, VD	748μs	865μs	1.6ms	2.0ms	3.0ms	134ms	
		001	SOC	201μs	230μs	405μs	501μs	754μs	34ms	
		010	ITMP							
		011	VA							
		100	VD**							

\*Note: Valid options for CHST in ADSTAT command are 0-4. If CHST is set to 5/6 in ADSTAT command, the LTC6804 treats it like ADAX command with CHG = 5/6.

\*\*The use of the ADSTAT command with CHST = 100 is not recommended unless special care is taken. See the Data Acquisition System Diagnostics section for more details.

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**Table 36. Configuration Register Group**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CFGR0	RD/WR	GPI05	GPI04	GPI03	GPI02	GPI01	REFON	SWTRD	ADCOPT
CFGR1	RD/WR	VUV[7]	VUV[6]	VUV[5]	VUV[4]	VUV[3]	VUV[2]	VUV[1]	VUV[0]
CFGR2	RD/WR	VOV[3]	VOV[2]	VOV[1]	VOV[0]	VUV[11]	VUV[10]	VUV[9]	VUV[8]
CFGR3	RD/WR	VOV[11]	VOV[10]	VOV[9]	VOV[8]	VOV[7]	VOV[6]	VOV[5]	VOV[4]
CFGR4	RD/WR	DCC8	DCC7	DCC6	DCC5	DCC4	DCC3	DCC2	DCC1
CFGR5	RD/WR	DCT0[3]	DCT0[2]	DCT0[1]	DCT0[0]	DCC12	DCC11	DCC10	DCC9

**Table 37. Cell Voltage Register Group A**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CVAR0	RD	C1V[7]	C1V[6]	C1V[5]	C1V[4]	C1V[3]	C1V[2]	C1V[1]	C1V[0]
CVAR1	RD	C1V[15]	C1V[14]	C1V[13]	C1V[12]	C1V[11]	C1V[10]	C1V[9]	C1V[8]
CVAR2	RD	C2V[7]	C2V[6]	C2V[5]	C2V[4]	C2V[3]	C2V[2]	C2V[1]	C2V[0]
CVAR3	RD	C2V[15]	C2V[14]	C2V[13]	C2V[12]	C2V[11]	C2V[10]	C2V[9]	C2V[8]
CVAR4	RD	C3V[7]	C3V[6]	C3V[5]	C3V[4]	C3V[3]	C3V[2]	C3V[1]	C3V[0]
CVAR5	RD	C3V[15]	C3V[14]	C3V[13]	C3V[12]	C3V[11]	C3V[10]	C3V[9]	C3V[8]

**Table 38. Cell Voltage Register Group B**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CVBR0	RD	C4V[7]	C4V[6]	C4V[5]	C4V[4]	C4V[3]	C4V[2]	C4V[1]	C4V[0]
CVBR1	RD	C4V[15]	C4V[14]	C4V[13]	C4V[12]	C4V[11]	C4V[10]	C4V[9]	C4V[8]
CVBR2	RD	C5V[7]	C5V[6]	C5V[5]	C5V[4]	C5V[3]	C5V[2]	C5V[1]	C5V[0]
CVBR3	RD	C5V[15]	C5V[14]	C5V[13]	C5V[12]	C5V[11]	C5V[10]	C5V[9]	C5V[8]
CVBR4	RD	C6V[7]	C6V[6]	C6V[5]	C6V[4]	C6V[3]	C6V[2]	C6V[1]	C6V[0]
CVBR5	RD	C6V[15]	C6V[14]	C6V[13]	C6V[12]	C6V[11]	C6V[10]	C6V[9]	C6V[8]

**Table 39. Cell Voltage Register Group C**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CVCR0	RD	C7V[7]	C7V[6]	C7V[5]	C7V[4]	C7V[3]	C7V[2]	C7V[1]	C7V[0]
CVCR1	RD	C7V[15]	C7V[14]	C7V[13]	C7V[12]	C7V[11]	C7V[10]	C7V[9]	C7V[8]
CVCR2	RD	C8V[7]	C8V[6]	C8V[5]	C8V[4]	C8V[3]	C8V[2]	C8V[1]	C8V[0]
CVCR3	RD	C8V[15]	C8V[14]	C8V[13]	C8V[12]	C8V[11]	C8V[10]	C8V[9]	C8V[8]
CVCR4	RD	C9V[7]	C9V[6]	C9V[5]	C9V[4]	C9V[3]	C9V[2]	C9V[1]	C9V[0]
CVCR5	RD	C9V[15]	C9V[14]	C9V[13]	C9V[12]	C9V[11]	C9V[10]	C9V[9]	C9V[8]

**Table 40. Cell Voltage Register Group D**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
CVDR0	RD	C10V[7]	C10V[6]	C10V[5]	C10V[4]	C10V[3]	C10V[2]	C10V[1]	C10V[0]
CVDR1	RD	C10V[15]	C10V[14]	C10V[13]	C10V[12]	C10V[11]	C10V[10]	C10V[9]	C10V[8]
CVDR2	RD	C11V[7]	C11V[6]	C11V[5]	C11V[4]	C11V[3]	C11V[2]	C11V[1]	C11V[0]
CVDR3	RD	C11V[15]	C11V[14]	C11V[13]	C11V[12]	C11V[11]	C11V[10]	C11V[9]	C11V[8]
CVDR4	RD	C12V[7]	C12V[6]	C12V[5]	C12V[4]	C12V[3]	C12V[2]	C12V[1]	C12V[0]
CVDR5	RD	C12V[15]	C12V[14]	C12V[13]	C12V[12]	C12V[11]	C12V[10]	C12V[9]	C12V[8]

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**Table 41. Auxiliary Register Group A**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
AVAR0	RD	G1V[7]	G1V[6]	G1V[5]	G1V[4]	G1V[3]	G1V[2]	G1V[1]	G1V[0]
AVAR1	RD	G1V[15]	G1V[14]	G1V[13]	G1V[12]	G1V[11]	G1V[10]	G1V[9]	G1V[8]
AVAR2	RD	G2V[7]	G2V[6]	G2V[5]	G2V[4]	G2V[3]	G2V[2]	G2V[1]	G2V[0]
AVAR3	RD	G2V[15]	G2V[14]	G2V[13]	G2V[12]	G2V[11]	G2V[10]	G2V[9]	G2V[8]
AVAR4	RD	G3V[7]	G3V[6]	G3V[5]	G3V[4]	G3V[3]	G3V[2]	G3V[1]	G3V[0]
AVAR5	RD	G3V[15]	G3V[14]	G3V[13]	G3V[12]	G3V[11]	G3V[10]	G3V[9]	G3V[8]

**Table 42. Auxiliary Register Group B**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
AVBR0	RD	G4V[7]	G4V[6]	G4V[5]	G4V[4]	G4V[3]	G4V[2]	G4V[1]	G4V[0]
AVBR1	RD	G4V[15]	G4V[14]	G4V[13]	G4V[12]	G4V[11]	G4V[10]	G4V[9]	G4V[8]
AVBR2	RD	G5V[7]	G5V[6]	G5V[5]	G5V[4]	G5V[3]	G5V[2]	G5V[1]	G5V[0]
AVBR3	RD	G5V[15]	G5V[14]	G5V[13]	G5V[12]	G5V[11]	G5V[10]	G5V[9]	G5V[8]
AVBR4	RD	REF[7]	REF[6]	REF[5]	REF[4]	REF[3]	REF[2]	REF[1]	REF[0]
AVBR5	RD	REF[15]	REF[14]	REF[13]	REF[12]	REF[11]	REF[10]	REF[9]	REF[8]

**Table 43. Status Register Group A**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
STAR0	RD	SOC[7]	SOC[6]	SOC[5]	SOC[4]	SOC[3]	SOC[2]	SOC[1]	SOC[0]
STAR1	RD	SOC[15]	SOC[14]	SOC[13]	SOC[12]	SOC[11]	SOC[10]	SOC[9]	SOC[8]
STAR2	RD	ITMP[7]	ITMP[6]	ITMP[5]	ITMP[4]	ITMP[3]	ITMP[2]	ITMP[1]	ITMP[0]
STAR3	RD	ITMP[15]	ITMP[14]	ITMP[13]	ITMP[12]	ITMP[11]	ITMP[10]	ITMP[9]	ITMP[8]
STAR4	RD	VA[7]	VA[6]	VA[5]	VA[4]	VA[3]	VA[2]	VA[1]	VA[0]
STAR5	RD	VA[15]	VA[14]	VA[13]	VA[12]	VA[11]	VA[10]	VA[9]	VA[8]

**Table 44. Status Register Group B**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
STBR0	RD	VD[7]	VD[6]	VD[5]	VD[4]	VD[3]	VD[2]	VD[1]	VD[0]
STBR1	RD	VD[15]	VD[14]	VD[13]	VD[12]	VD[11]	VD[10]	VD[9]	VD[8]
STBR2	RD	C40V	C4UV	C30V	C3UV	C20V	C2UV	C10V	C1UV
STBR3	RD	C80V	C8UV	C70V	C7UV	C60V	C6UV	C50V	C5UV
STBR4	RD	C120V	C12UV	C110V	C11UV	C100V	C10UV	C90V	C9UV
STBR5	RD	REV[3]	REV[2]	REV[1]	REV[0]	RSVD	RSVD	MUXFAIL	THSD

**Table 45. COMM Register Group**

REGISTER	RD/WR	BIT 7	BIT 6	BIT 5	BIT 4	BIT 3	BIT 2	BIT 1	BIT 0
COMM0	RD/WR	ICOM0[3]	ICOM0[2]	ICOM0[1]	ICOM0[0]	D0[7]	D0[6]	D0[5]	D0[4]
COMM1	RD/WR	D0[3]	D0[2]	D0[1]	D0[0]	FCOM0[3]	FCOM0[2]	FCOM0[1]	FCOM0[0]
COMM2	RD/WR	ICOM1[3]	ICOM1[2]	ICOM1[1]	ICOM1[0]	D1[7]	D1[6]	D1[5]	D1[4]
COMM3	RD/WR	D1[3]	D1[2]	D1[1]	D1[0]	FCOM1[3]	FCOM1[2]	FCOM1[1]	FCOM1[0]
COMM4	RD/WR	ICOM2[3]	ICOM2[2]	ICOM2[1]	ICOM2[0]	D2[7]	D2[6]	D2[5]	D2[4]
COMM5	RD/WR	D2[3]	D2[2]	D2[1]	D2[0]	FCOM2[3]	FCOM2[2]	FCOM2[1]	FCOM2[0]

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**Table 46. Memory Bit Descriptions**

NAME	DESCRIPTION	VALUES																
GPIOx	GPIOx Pin Control	Write: 0 -> GPIOx Pin Pull-Down ON; 1-> GPIOx Pin Pull-Down OFF (Default) Read: 0 -> GPIOx Pin at Logic 0; 1 -> GPIOx Pin at Logic 1																
REFON	Reference Powered Up	1 -> Reference Remains Powered Up Until Watchdog Timeout 0 -> Reference Shuts Down after Conversions (Default)																
SWTRD	SWTEN Pin Status (Read Only)	1 -> SWTEN Pin at Logic 1 0 -> SWTEN Pin at Logic 0																
ADCOPT	ADC Mode Option Bit	ADCOPT: 0 -> Selects Modes 27kHz, 7kHz or 26Hz with MD[1:0] Bits in ADC Conversion Commands (Default). 1 -> Selects Modes 14kHz, 3kHz or 2kHz with MD[1:0] Bits in ADC Conversion Commands.																
VUV	Undervoltage Comparison Voltage*	Comparison voltage = (VUV + 1) • 16 • 100µV Default: VUV = 0x000																
VOV	Overvoltage Comparison Voltage*	Comparison voltage = VOV • 16 • 100µV Default: VOV = 0x000																
DCC[x]	Discharge Cell x	x = 1 to 12 1 -> Turn ON Shorting Switch for Cell x 0 -> Turn OFF Shorting Switch for Cell x (Default)																
DCTO	Discharge Time Out Value	DCTO (Write)	0	1	2	3	4	5	6	7	8	9	A	B	C	D	E	F
		Time (Min)	Disabled	0.5	1	2	3	4	5	10	15	20	30	40	60	75	90	120
		DCTO (Read)	0	1	2	3	4	5	6	7	8	9	A	B	C	D	E	F
		Time Left (Min)	Disabled or Timeout	0 to 0.5	0.5 to 1	1 to 2	2 to 3	3 to 4	4 to 5	5 to 10	10 to 15	15 to 20	20 to 30	30 to 40	40 to 60	60 to 75	75 to 90	90 to 120
CxV	Cell x Voltage*	x = 1 to 12 16-Bit ADC Measurement Value for Cell x Cell Voltage for Cell x = CxV • 100µV CxV Is Reset to 0xFFFF on Power-Up and After Clear Command																
GxV	GPIO x Voltage*	x = 1 to 5 16-Bit ADC Measurement Value for GPIOx Voltage for GPIOx = GxV • 100µV GxV Is Reset to 0xFFFF on Power-Up and After Clear Command																
REF	2nd Reference Voltage*	16-Bit ADC Measurement Value for 2nd Reference Voltage for 2nd Reference = REF • 100µV <b>Normal Range Is within 2.985V to 3.015V</b>																
SOC	Sum of Cells Measurement*	16-Bit ADC Measurement Value of the Sum of All Cell Voltages Sum of All Cells Voltage = SOC • 100µV • 20																
ITMP	Internal Die Temperature*	16-Bit ADC Measurement Value of Internal Die Temperature <b>Temperature Measurement (°C) = ITMP • 100µV/7.5mV/°C – 273°C</b>																
VA	Analog Power Supply Voltage*	16-Bit ADC Measurement Value of Analog Power Supply Voltage Analog Power Supply Voltage = VA • 100µV <b>Normal Range Is within 4.5V to 5.5V</b>																
VD	Digital Power Supply Voltage*	16-Bit ADC Measurement Value of Digital Power Supply Voltage Digital Power Supply Voltage = VA • 100µV <b>Normal Range Is within 2.7V to 3.6V</b>																
CxOV	Cell x Overvoltage Flag	x = 1 to 12 Cell Voltage Compared to VOV Comparison Voltage 0 -> Cell x Not Flagged for Overvoltage Condition. 1 -> Cell x Flagged																
CxUV	Cell x Undervoltage Flag	x = 1 to 12 Cell Voltage Compared to VUV Comparison Voltage 0 -> Cell x Not Flagged for Undervoltage Condition. 1 -> Cell x Flagged																
REV	Revision Code	Device Revision Code. See Revision Code and Reserved Bits in Operation Section.																
RSVD	Reserved Bits	See Revision Code and Reserved Bits in Operation Section.																

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**Table 46. Memory Bit Descriptions**

NAME	DESCRIPTION	VALUES						
MUXFAIL	Multiplexer Self-Test Result	Read: 0 -> Multiplexer Passed Self Test   1 -> Multiplexer Failed Self Test						
THSD	Thermal Shutdown Status	Read: 0 -> Thermal Shutdown Has Not Occurred   1 -> Thermal Shutdown Has Occurred THSD Bit Cleared to 0 on Read of Status Register Group B						
ICOMn	Initial Communication Control Bits	Write	I2C	0110	0001	0000	0111	
				START	STOP	BLANK	NO TRANSMIT	
			SPI	1000	1001	1111		
				CSB Low	CSB High	NO TRANSMIT		
		Read	I2C	0110	0001	0000	0111	
				START from Master	STOP from Master	SDA Low Between Bytes	SDA High Between Bytes	
			SPI	0111				
Dn	I <sup>2</sup> C/SPI Communication Data Byte	Data Transmitted (Received) to (From) I <sup>2</sup> C/SPI Slave Device						
FCOMn	Final Communication Control Bits	Write	I2C	0000	1000	1001		
				Master ACK	Master NACK	Master NACK + STOP		
			SPI	X000	1001			
				CSB Low	CSB High			
		Read	I2C	0000	0111	1111	0001	1001
				ACK from Master	ACK from Slave	NACK from Slave	ACK from Slave + STOP from Master	NACK from Slave + STOP from Master
			SPI	1111				

\*Voltage equations use the decimal value of registers, 0 to 4095 for 12 bits and 0 to 65535 for 16 bits.

## PROGRAMMING EXAMPLES

The following examples use a configuration of 3 stacked LTC6804-1 devices: S1, S2, S3. Port A on device S1 is configured in SPI mode (ISOMD pin low). Port A on devices S2 and S3 is configured in isoSPI mode (ISOMD pin high). Port B on S1 is connected to Port A on S2. Port B on S2 is connected to Port A on S3. The microcontroller communicates to the stack through Port A on S1.

### Waking Up Serial Interface

1. Send a dummy byte. The activity on CSB and SCK will wake up the serial interface on device S1.
2. Wait for the amount of time  $3 \cdot t_{WAKE}$  in order to power up all devices S1, S2 and S3.

For large stacks where some devices may go to the IDLE state after waking, apply steps 3 and 4:

3. Send a second dummy byte.

4. Wait for the amount of time  $3 \cdot t_{READY}$

5. Send commands

### Write Configuration Registers

1. Pull CSB low
2. Send WRCFG command (0x00 0x01) and its PEC (0x3D 0x6E)
3. Send CFGR0 byte of device S3, then CFGR1(S3), ... CFGR5(S3), PEC of CFGR0(S3) to CFGR5(S3)
4. Send CFGR0 byte of device S2, then CFGR1(S2), ... CFGR5(S2), PEC of CFGR0(S2) to CFGR5(S2)
5. Send CFGR0 byte of device S1, then CFGR1(S1), ... CFGR5(S1), PEC of CFGR0(S1) to CFGR5(S1)
6. Pull CSB high, data latched into all devices on rising edge of CSB



## OPERATION

Calculation of serial interface time for sequence above:

Number of LTC6804-1s in daisy chain stack =  $n$

Number of bytes in sequence (B):

Command: 2 (command byte) + 2 (command PEC) = 4

Data: 6 (Data bytes) + 2 (Data PEC) per LTC6804 = 8 bytes per device

$B = 4 + 8 \cdot n$

Serial port frequency per bit = F

Time =  $(1/F) \cdot B \cdot 8 \text{ bits/byte} = (1/F) \cdot [4 + 8 \cdot n] \cdot 8$

Time for 3 LTC6804 example above, with 1MHz serial port =  $(1/1\text{e}6) \cdot (4 + 8 \cdot 3) \cdot 8 = 224\mu\text{s}$

Note: This time will remain the same for all write and read commands.

### Read Cell Voltage Register Group A

1. Pull CSB low
2. Send RDCVA command (0x00 0x04) and its PEC (0x07 0xC2)
3. Read CVAR0 byte of device S1, then CVAR1(S1), ... CVAR5(S1), PEC of CVAR0(S1) to CVAR5(S1)
4. Read CVAR0 byte of device S2, then CVAR1(S2), ... CVAR5(S2), PEC of CVAR0(S2) to CVAR0(S2)
5. Read CVAR0 byte of device S3, then CVAR1(S3), ... CVAR5(S3), PEC of CVAR0(S3) to CVAR5(S3)
6. Pull CSB high

### Start Cell Voltage ADC Conversion

(All cells, normal mode with discharge permitted) and poll status

1. Pull CSB low
2. Send ADCV command with MD[1:0] = 10 and DCP = 1 i.e. 0x03 0x70 and its PEC (0xAF 0x42)
3. Pull CSB high

### Clear Cell Voltage Registers

1. Pull CSB low
2. Send CLRCELL command (0x07 0x11) and its PEC (0xC9 0xC0)
3. Pull CSB high

### Poll ADC Status

(Parallel configuration and ISOMD = 0)

This example uses an addressed LTC6804-2 with address A [3:0] = 0011 and ISOMD = 0

1. Pull CSB low
2. Send PLADC command (0x9F 0x14) and its PEC (0x1C 0x48 )
3. SDO output is pulled low if the LTC6804-2 is busy. The host needs to send clocks on SCK in order for the polling status to be updated from the addressed device.
4. SDO output is high when the LTC6804-2 has completed conversions
5. Pull CSB high to exit polling

### Talk to an I<sup>2</sup>C Slave Connected to LTC6804

The LTC6804 supports I<sup>2</sup>C slave devices by connection to GPIO4(SDA) and GPIO5(SCL). One valuable use for this capability is to store production calibration constants or other information in a small serial EEPROM using a connection like shown in Figure 25.

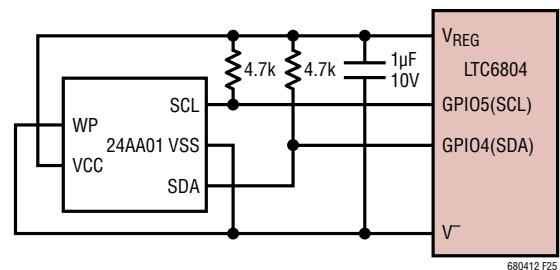


Figure 25. Connecting I<sup>2</sup>C EEPROM to LTC6804 GPIO Pins

## OPERATION

This example uses a single LTC6804-1 to write a byte of data to an I<sup>2</sup>C EEPROM. The LTC6804 will send three bytes of data to the I<sup>2</sup>C slave device. The data sent will be B0 = 0xA0 (EEPROM address), B1 = 0x01 (write command), and B2 = 0xAA (data to be stored in EEPROM). The three bytes will be transmitted to the I<sup>2</sup>C slave device in the following format:

START – B0 – NACK – B1 – NACK – B2 – NACK – STOP

### 1. Write data to COMM register using WRCOMM command

- Pull CSB low
- Send WRCOMM command (0x07 0x21) and its PEC (0x24 0xB2)
- Send  
COMM0 = 0x6A, COMM1 = 0x08 ([START] [B0] [NACK]),  
COMM2 = 0x00, COMM3 = 0x18 ([BLANK] [B1] [NACK]),  
COMM4 = 0x0A, COMM5 = 0xA9 ([BLANK] [B2] [NACK+STOP])  
and PEC = 0x6D 0xFB for the above data
- Pull CSB high

### 2. Send the 3 bytes of data to I<sup>2</sup>C slave device using STCOMM command

- Pull CSB low
- Send STCOMM command (0x07 0x23) and its PEC (0xB9 0xE4)
- Send 72 clock cycles on SCK
- Pull CSB high

### 3. Data transmitted to slave during the STCOMM command is stored in the COMM register. Use the RDCOMM command to retrieve the data

- Pull CSB low
- Send RDCOMM command (0x07 0x22) and its PEC (0x32 0xD6)
- Read COMM0-COMM5 and the PEC for the 6 bytes of data.

Assuming the slave acknowledged all 3 bytes of data, the read back data in this example would look like:

COMM0 = 0x6A, COMM1 = 0x07, COMM2 = 0x70,  
COMM3 = 0x17, COMM4 = 0x7A, COMM5 = 0xA1,  
PEC = 0xD0 0xDE

- Pull CSB high

Note: If the slave returns data, this data will be placed in COMM0-COMM5.

Figure 26 shows the activity on GPIO5 (SCL) and GPIO4 (SDA) ports of the I<sup>2</sup>C master for 72 clock cycles during the STCOMM command in the above example.

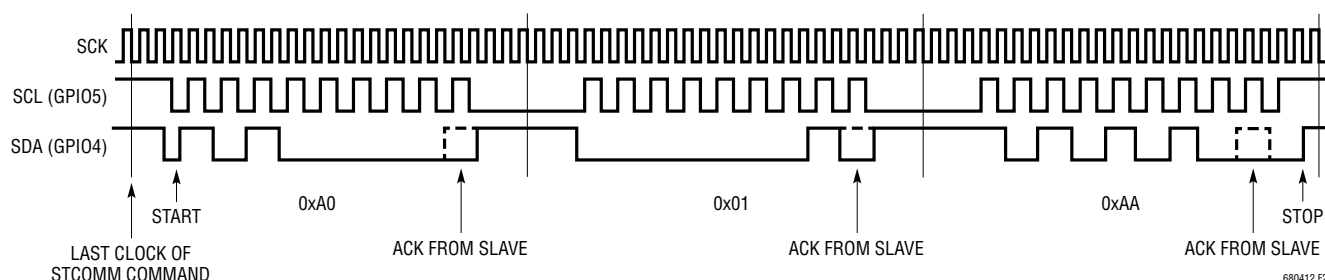


Figure 26. LTC6804 I<sup>2</sup>C Communication Example

## OPERATION

### Talk to a SPI Slave Connected to LTC6804

This example uses a single LTC6804-1 device which has a SPI device connected to it through GPIO3 (CSBM), GPIO4 (SDOM) and GPIO5 (SCKM). In this example, the LTC6804 device sends out 3 bytes of data B0 = 0x55, B1 = 0xAA and B2 = 0xCC to the SPI slave device in the following format: CSB low – B0 – B1 – B2 – CSB high

1. Write data to COMM register using WRCOMM command
  - a. Pull CSBM low
  - b. Send WRCOMM command (0x07 0x21) and its PEC (0x24 0xB2)
  - c. Send  
 COMM0 = 0x85, COMM1 = 0x50 ([CSBM low] [B0] [CSBM low]),  
 COMM2 = 0x8A, COMM3 = 0xA0 ([CSBM low] [B1] [CSBM low]),  
 COMM4 = 0x8C, COMM5 = 0xC9 ([CSBM low] [B2] [CSBM high])  
 and PEC = 0x89 0xA4 for the above data.
  - d. Pull CSB high
2. Send the 3 bytes of data to SPI slave device using STCOMM command
  - a. Pull CSB low
  - b. Send STCOMM command (0x07 0x23) and its PEC (0xB9 0xE4)
  - c. Send 72 clock cycles on SCK
  - d. Pull CSB high

3. Data transmitted to slave during the STCOMM command is stored in the COMM register. Use the RDCOMM command to retrieve the data.

- a. Pull CSB low
- b. Send RDCOMM command (0x07 0x22) and its PEC (0x32 0xD6)
- c. Read COMM0-COMM5 and the PEC for the 6 bytes of data. The read back data in this example would look like:  
 COMM0 = 0x755F, COMM1 = 0x7AAF, COMM2 = 7CCF, PEC = 0xF2BA
- d. Pull CSB high

Note: If the slave returns data, this data will be placed in COMM0-COMM5.

Figure 27 shows the activity on GPIO3 (CSBM), GPIO5 (SCKM) and GPIO4 (SDOM) ports of SPI master for 72 clock cycles during the STCOMM command in the above example.

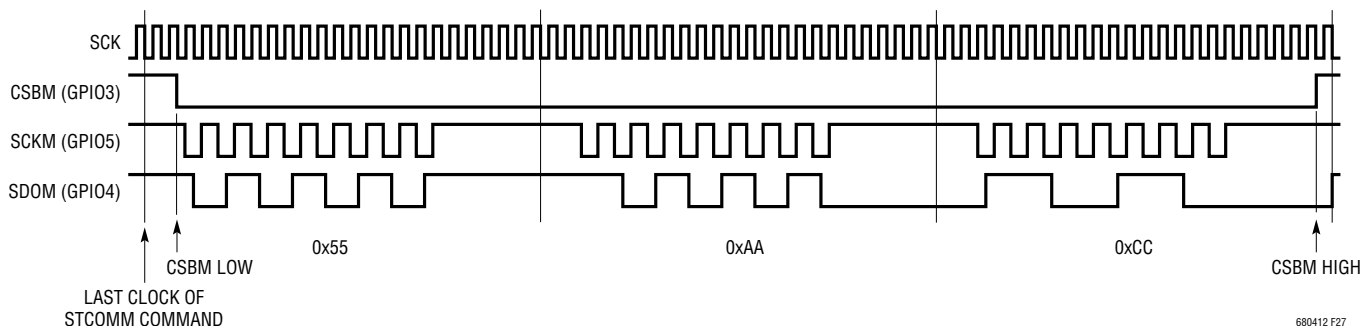


Figure 27. LTC6804 SPI Communication Example

## APPLICATIONS INFORMATION

### SIMPLE LINEAR REGULATOR

The LTC6804 draws most of its power from the  $V_{REG}$  input pin.  $5V \pm 0.5V$  should be applied to  $V_{REG}$ . A regulated DC/DC converter can power  $V_{REG}$  directly, or the DRIVE pin may be used to form a discrete regulator with the addition of a few external components. When active, the DRIVE output pin provides a low current 5.6V output that can be buffered using a discrete NPN transistor, as shown in Figure 28. The collector power for the NPN can come from any potential of 6V or more above  $V^-$ , including the cells being monitored or an unregulated converter supply. A  $100\Omega/100nF$  RC decoupling network is recommended for the collector power connection to protect the NPN from transients. The emitter of the NPN should be bypassed with a  $1\mu F$  capacitor. Larger capacitor values should be avoided because they increase the wake-up time of the LTC6804. Some attention to the thermal characteristic of the NPN is needed, as there can be significant heating with a high collector voltage.

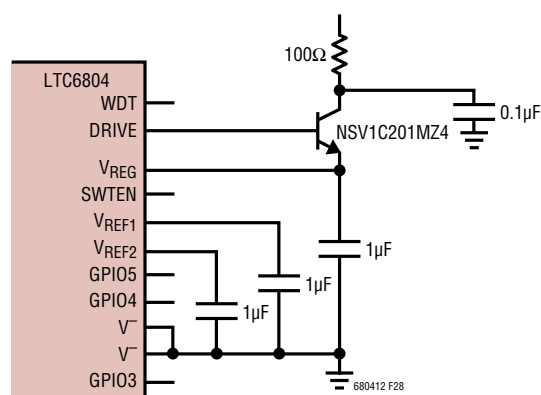


Figure 28. Simple  $V_{REG}$  Power Source Using NPN Pass Transistor

### IMPROVED REGULATOR POWER EFFICIENCY

To minimize power consumption within the LTC6804, the current drawn on the  $V^+$  pin has been designed to be very small ( $500\mu A$ ). The voltage on the  $V^+$  pin must be at least as high as the top cell to provide accurate measurement. The  $V^+$  and  $V_{REG}$  pins can be unpowered to provide an exceptionally low battery drain shutdown mode. In many applications, the  $V^+$  will be permanently connected to the top cell potential through a decoupling RC to protect against transients ( $100\Omega/100nF$  is recommended).

For better running efficiency when powering from the cell stack, the  $V_{REG}$  may be powered from a buck converter rather than the NPN pass transistor. An ideal circuit for this is based on the LT3990 as shown in Figure 29. A  $1k$  resistor should be used in series with the input to prevent inrush current when connecting to the stack and to reduce conducted EMI. The EN/UVLO pin should be connected to DRIVE so that the converter sleeps along with the LTC6804. The LTC6804 watchdog timer requires  $V_{REG}$  power to timeout. Therefore, if the EN/UVLO pin is not connected to DRIVE, care must be taken to allow the LTC6804 to timeout first before removing  $V_{REG}$  power; otherwise the LTC6804 will not enter sleep mode.

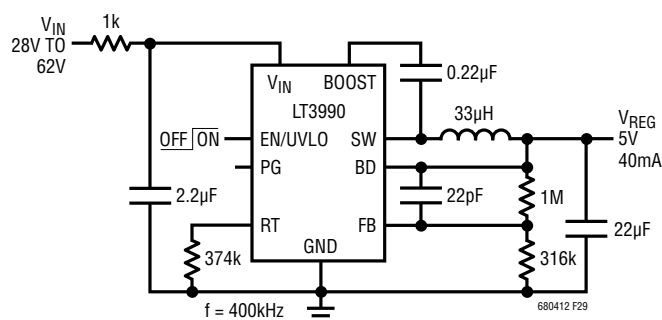


Figure 29.  $V_{REG}$  Powered from Cell Stack with High Efficiency

## APPLICATIONS INFORMATION

### FULLY ISOLATED POWER

A simple DC/DC flyback converter can provide isolated power for an LTC6804 from a remote 12V power source as shown in Figure 30. This circuit, along with the isoSPI transformer isolation, results in LTC6804 circuitry that is completely floating and uses almost no power from the batteries. Aside from reducing the amount of circuitry that operates at battery potential, such an arrangement prevents battery load imbalance. The LTC6804 watchdog timer requires  $V_{REG}$  power to timeout. Therefore, care must be taken to allow the LTC6804 to timeout first before removing  $V_{REG}$  power; otherwise the LTC6804 will not enter sleep mode. A diode should be added between the  $V+$  and the top cell being monitored. This will prevent any

current from conducting through internal parasitic paths inside the IC when the isolated power is removed.

### READING EXTERNAL TEMPERATURE PROBES

Figure 31 shows the typical biasing circuit for a negative-temperature-coefficient (NTC) thermistor. The  $10k\Omega$  at  $25^\circ\text{C}$  is the most popular sensor value and the  $V_{REF2}$  output stage is designed to provide the current required to directly bias several of these probes. The biasing resistor is selected to correspond to the NTC value so the circuit will provide 1.5V at  $25^\circ\text{C}$  ( $V_{REF2}$  is 3V nominal). The overall circuit response is approximately  $-1\%/^\circ\text{C}$  in the range of typical cell temperatures, as shown in the chart of Figure 31.

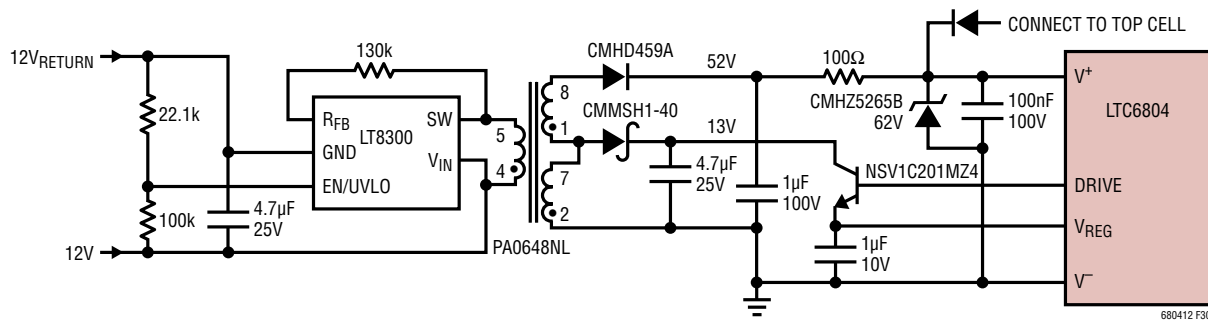


Figure 30. Powering LTC6804 from a Remote 12V Source

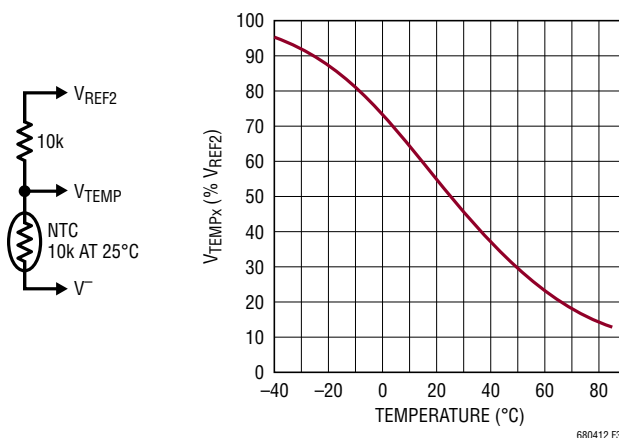


Figure 31. Typical Temperature Probe Circuit and Relative Output

## APPLICATIONS INFORMATION

### EXPANDING THE NUMBER OF AUXILIARY MEASUREMENTS

The LTC6804 provides five GPIO pins, each of which is capable of performing as an ADC input. In some applications there is need to measure more signals than this, so one means of supporting higher signal count is to add a MUX circuit such as shown in Figure 32. This circuit digitizes up to sixteen source signals using the GPIO1 ADC input and MUX control is provided by two other GPIO lines configured as an I<sup>2</sup>C port. The buffer amplifier provides for fast settling of the selected signal to increase the usable conversion rate.

### INTERNAL PROTECTION FEATURES

The LTC6804 incorporates various ESD safeguards to ensure a robust performance. An equivalent circuit showing the specific protection structures is shown in Figure 33. While pins 43 to 48 have different functionality for the -1 and -2 variants, the protection structure is the same. Zener-like suppressors are shown with their nominal clamp voltage, other diodes exhibit standard PN junction behavior.

### FILTERING OF CELL AND GPIO INPUTS

The LTC6804 uses a delta-sigma ADC, which has delta-sigma modulator followed by a SINC3 finite impulse response (FIR) digital filter. This greatly reduces input filtering requirements. Furthermore, the programmable oversampling ratio allows the user to determine the best trade-off between measurement speed and filter cutoff frequency. Even with this high order lowpass filter, fast transient noise can still induce some residual noise in measurements, especially in the faster conversion modes. This can be minimized by adding an RC lowpass decoupling to each ADC input, which also helps reject potentially damaging high energy transients. Adding more than about 100Ω to the ADC inputs begins to introduce a systematic error in the measurement, which can be improved by raising the filter capacitance or mathematically compensating in software with a calibration procedure. For situations that demand the highest level of battery voltage ripple rejection, grounded capacitor filtering is recommended. This configuration has a series resistance and capacitors that decouple HF noise to V<sup>-</sup>. In systems where noise is less

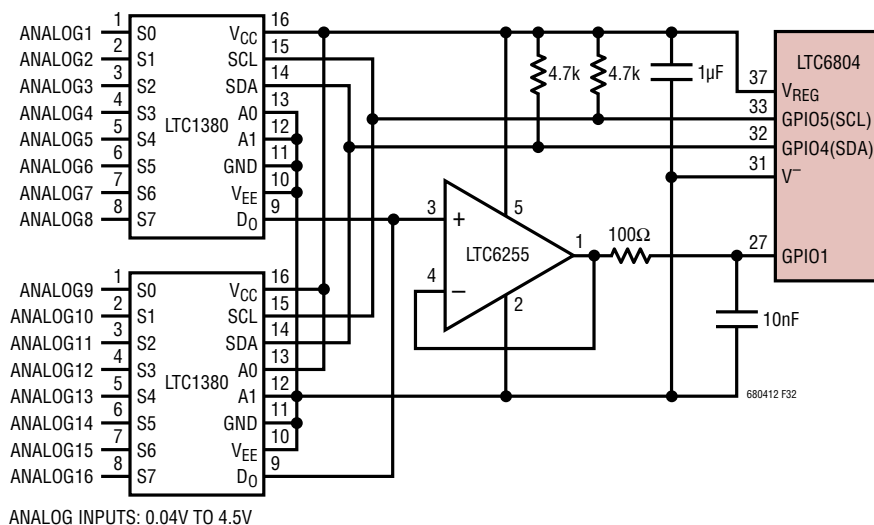


Figure 32. MUX Circuit Supports Sixteen Additional Analog Measurements

## APPLICATIONS INFORMATION

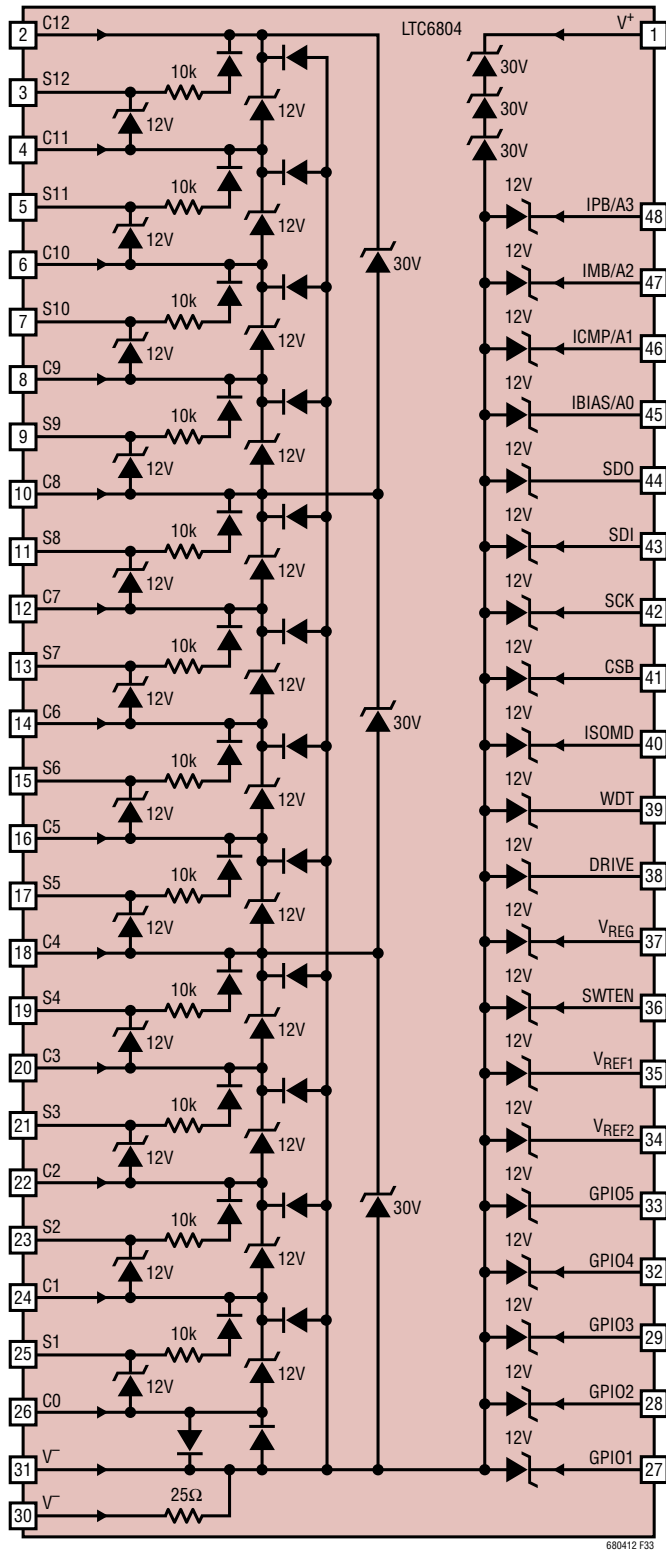


Figure 33. Internal ESD Protection Structure of LTC6804

periodic or higher oversample rates are in use, a differential capacitor filter structure is adequate. In this configuration there are series resistors to each input, but the capacitors connect between the adjacent C pins. However, the differential capacitor sections interact. As a result, the filter response is less consistent and results in less attenuation than predicted by the RC, by approximately a decade. Note that the capacitors only see one cell of applied voltage (thus smaller and lower cost) and tend to distribute transient energy uniformly across the IC (reducing stress events on the internal protection structure). Figure 34 shows the two methods schematically. Basic ADC accuracy varies with R, C as shown in the Typical Performance curves, but error is minimized if  $R = 100\Omega$  and  $C = 10\text{nF}$ . The GPIO pins will always use a grounded capacitor configuration because the measurements are all with respect to  $V^-$ .

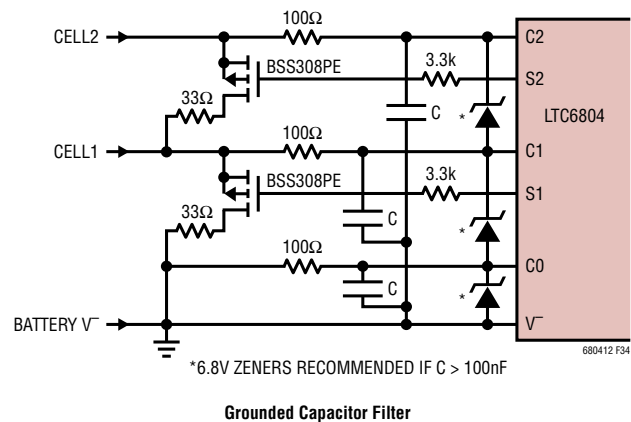
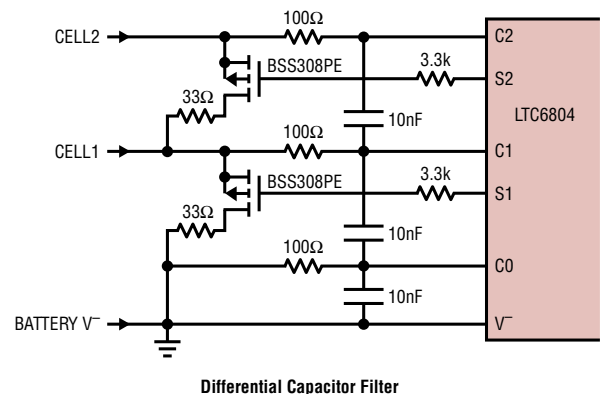


Figure 34. Input Filter Structure Configurations



## APPLICATIONS INFORMATION

### CELL BALANCING WITH INTERNAL MOSFETS

The S1 through S12 pins are used to balance battery cells. If one cell in a series becomes overcharged, an S output can be used to discharge the cell. Each S output has an internal N-channel MOSFET for discharging. The NMOS has a maximum on resistance of 20Ω. An external resistor should be connected in series with the NMOS to dissipate heat outside of the LTC6804 package as illustrated in Figure 35. It is still possible to use an RC to add additional filtering to cell voltage measurements but the filter R must remain small, typically around 10Ω to reduce the effect on the programmed balance current. When using the internal MOSFETs to discharge cells, the die temperature should be monitored. See Power Dissipation and Thermal Shutdown section.

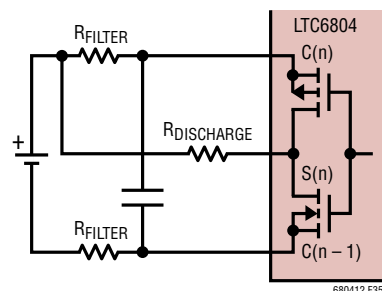


Figure 35. Internal Discharge Circuit

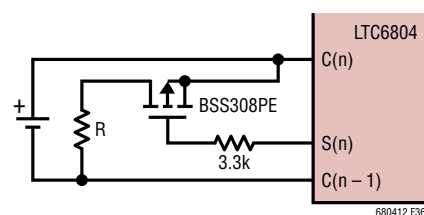


Figure 36. External Discharge Circuit

### CELL BALANCING WITH EXTERNAL MOSFETS

The S outputs include an internal pull-up PMOS transistor. The S pins can act as digital outputs suitable for driving the gate of an external MOSFET. For applications requiring high battery discharge currents, connect a discrete PMOS switch device and suitable discharge resistor to the cell, and the gate terminal to the S output pin, as illustrated in Figure 36. Figure 34 shows external MOSFET circuits that include RC filtering.

### DISCHARGE CONTROL DURING CELL MEASUREMENTS

If the discharge permitted (DCP) command bit is high in a cell measurement command, then the S pin discharge states are not altered during the cell measurements. However, if the DCP bit is low, any discharge that is turned on will be turned off when the corresponding cell or adjacent cells are being measured. Table 47 illustrates this during an

Table 47. Discharge Control During an ADCV Command with DCP = 0

DISCHARGE PIN	CELL MEASUREMENT PERIODS						CELL CALIBRATION PERIODS					
	CELL1/7	CELL2/8	CELL3/9	CELL4/10	CELL5/11	CELL6/12	CELL1/7	CELL2/8	CELL3/9	CELL4/10	CELL5/11	CELL6/12
	t <sub>0</sub> to t <sub>1M</sub>	t <sub>1M</sub> to t <sub>2M</sub>	t <sub>2M</sub> to t <sub>3M</sub>	t <sub>3M</sub> to t <sub>4M</sub>	t <sub>4M</sub> to t <sub>5M</sub>	t <sub>5M</sub> to t <sub>6M</sub>	t <sub>6M</sub> to t <sub>1C</sub>	t <sub>1C</sub> to t <sub>2C</sub>	t <sub>2C</sub> to t <sub>3C</sub>	t <sub>3C</sub> to t <sub>4C</sub>	t <sub>4C</sub> to t <sub>5C</sub>	t <sub>5C</sub> to t <sub>6C</sub>
S1	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF
S2	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON
S3	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON
S4	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON
S5	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF
S6	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF
S7	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF
S8	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON
S9	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON
S10	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF	ON
S11	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF	OFF
S12	OFF	ON	ON	ON	OFF	OFF	OFF	ON	ON	ON	OFF	OFF

680412fc

## APPLICATIONS INFORMATION

ADCV command with DCP = 0. In this table, OFF implies that a discharge is forced off during that period even if the corresponding DCC[x] bit is high in the configuration register. ON implies that if the discharge is turned on, it will stay on during that period. Refer to Figure 3 for the timing of the ADCV command.

### POWER DISSIPATION AND THERMAL SHUTDOWN

The internal MOSFETs connected to the pins S1 through S12 pins can be used to discharge battery cells. An external resistor should be used to limit the power dissipated by the MOSFETs. The maximum power dissipation in the MOSFETs is limited by the amount of heat that can be tolerated by the LTC6804. Excessive heat results in elevated die temperatures. Little or no degradation will be observed in the measurement accuracy for die temperatures up to 125°C. Damage may occur above 150°C, therefore the recommended maximum die temperature is 125°C. To protect the LTC6804 from damage due to overheating a thermal shutdown circuit is included. Overheating of the device can occur when dissipating significant power in the cell discharge switches. The thermal shutdown circuit is enabled whenever the device is not in sleep mode (see LTC6804 Core State Descriptions). If the temperature detected on the device goes above approximately 150°C the configuration registers will be reset to default states turning off all discharge switches. When a thermal shutdown has occurred, the THSD bit in the status register group B will go high. The bit is cleared after a read operation of the status register group B. The bit can also be set using the CLRSTAT command. Since thermal shutdown interrupts normal operation, the internal temperature monitor should be used to determine when the device temperature is approaching unacceptable levels.

### METHOD TO VERIFY BALANCING CIRCUITRY

The functionality of the discharge circuitry is best verified by cell measurements. Figure 37 shows an example using the LTC6804 battery monitor IC. The resistor between the battery and the source of the discharge MOSFET causes cell voltage measurements to decrease. The amount of measurement change depends on the resistor values and the MOSFET on resistance.

The following algorithm could be used in conjunction with Figure 37:

1. Measure all cells with no discharging (all S outputs off) and read and store the results.
2. Turn on S1 and S7
3. Measure C1-C0, C7-C6
4. Turn off S1 and S7
5. Turn on S2 and S8
6. Measure C2-C1, C8-C7
7. Turn off S2 and S8
- ...
14. Turn on S6 and S12
15. Measure C6-C5, C12-C11
16. Turn off S6 and S12
17. Read the voltage register group to get the results of steps 2 thru 16.
18. Compare new readings with old readings. Each cell voltage reading should have decreased by a fixed percentage set by  $R_{B1}$  and  $R_{B2}$  (Figure 37). The exact amount of decrease depends on the resistor values and MOSFET characteristics.

### Improved PEC Calculation

The PEC allows the user to have confidence that the serial data read from the LTC6804 is valid and has not been corrupted by any external noise source. This is a critical feature for reliable communication and the LTC6804 requires that a PEC be calculated for all data being read from and written to the LTC6804. For this reason it is important to have an efficient method for calculating the PEC. The code below demonstrates a simple implementation of a lookup table derived PEC calculation method. There are two functions, the first function `init_PEC15_Table()` should only be called once when the microcontroller starts and will initialize a PEC15 table array called `pec15Table[]`. This table will be used in all future PEC calculations. The `pec15` table can also be hard coded into the microcontroller rather than running the `init_PEC15_Table()` function at startup. The `pec15()` function calculates the PEC and will return the correct 15 bit PEC for byte arrays of any given length.

APPLICATIONS INFORMATION

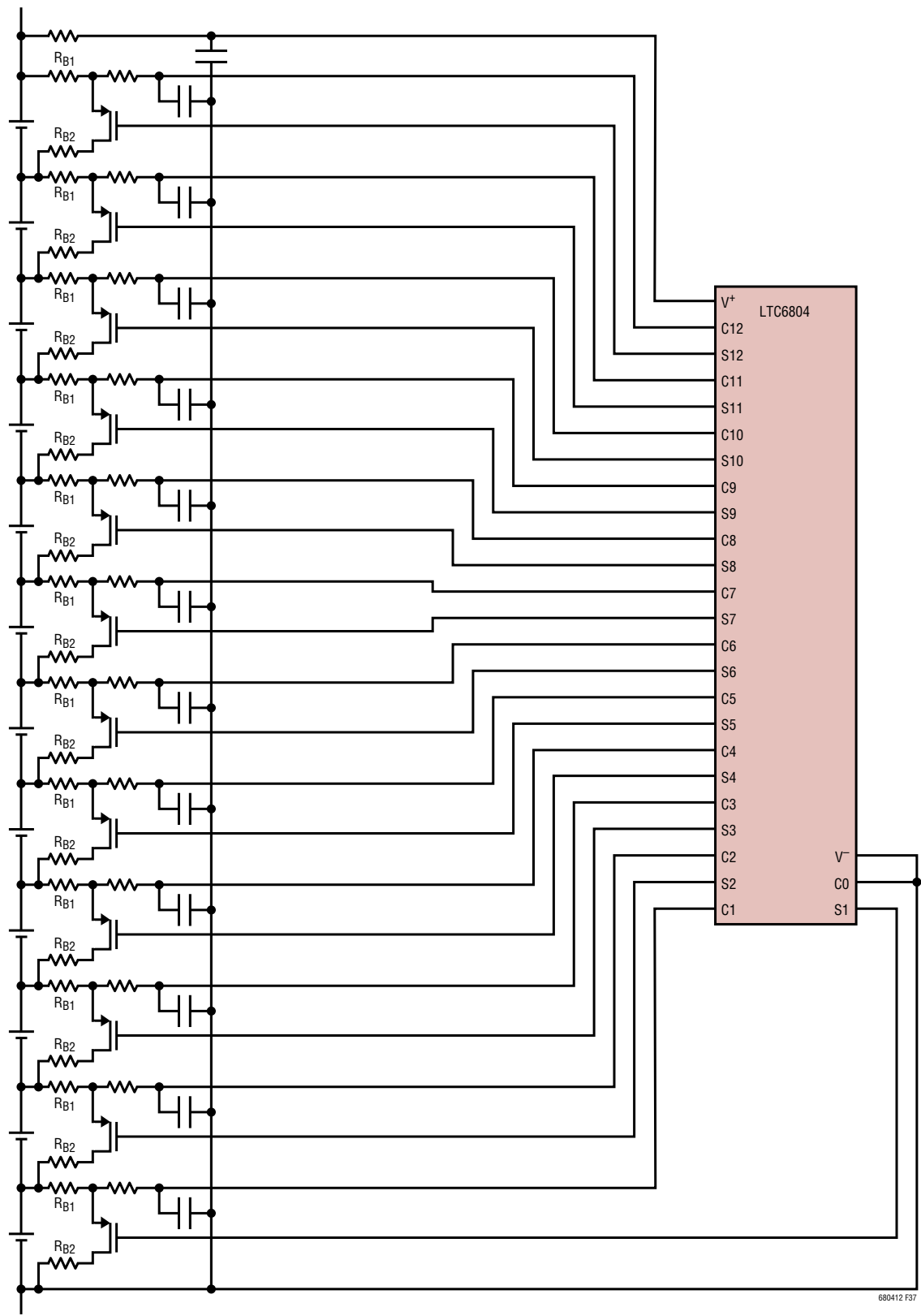


Figure 37. Balancing Self Test Circuit

## APPLICATIONS INFORMATION

/\*\*\*\*\*\*

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\*\*\*\*\*/

```
int16 pec15Table[256];
int16 CRC15_POLY = 0x4599;
void init_PEC15_Table()
{
    for (int i = 0; i < 256; i++)
    {
        remainder = i << 7;
        for (int bit = 8; bit > 0; --bit)
        {
            if (remainder & 0x4000)
            {
                remainder = ((remainder << 1));
                remainder = (remainder ^ CRC15poly)
            }
            else
            {
                remainder = ((remainder << 1));
            }
        }
        pec15Table[i] = remainder&0xFFFF;
    }
}

unsigned int16 pec15 (char *data , int len)
{
    int16 remainder,address;

    remainder = 16;//PEC seed
    for (int i = 0; i < len; i++)
    {
        address = ((remainder >> 7) ^ data[i]) & 0xff;//calculate PEC table address
        remainder = (remainder << 8 ) ^ pec15Table[address];
    }
    return (remainder*2);//The CRC15 has a 0 in the LSB so the final value must be multiplied by 2
}
```

## APPLICATIONS INFORMATION

### CURRENT MEASUREMENT WITH A HALL EFFECT SENSOR

The LTC6804 auxiliary ADC inputs (GPIO pins) may be used for any analog signal, including those from various active sensors that generate a compatible voltage. One such example that may be useful in a battery management setting is the capture of battery current. Hall-effect sensors are popular for measuring large battery currents since the technology provides a non-contact, low power dissipation solution. Figure 38 shows schematically a typical Hall sensor that produces two outputs that proportion to the  $V_{CC}$  provided. The sensor is powered from a 5V source

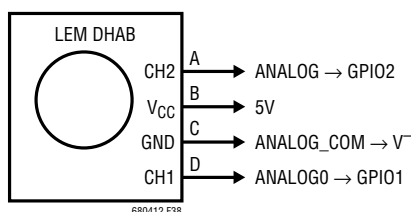


Figure 38. Interfacing a Typical Hall-Effect Battery Current Sensor to Auxiliary ADC Inputs

and produces analog outputs that are connected to GPIO pins or inputs of the MUX application shown in Figure 32. The use of GPIO1 and GPIO2 as the ADC inputs has the possibility of being digitized within the same conversion sequence as the cell inputs (using the ADCVAX command), thus synchronizing cell voltage and cell current measurements.

### CURRENT MEASUREMENT WITH A SHUNT RESISTOR

It is possible to measure the battery current on the LTC6804 GPIO pins with a high performance current sense amplifier and a shunt. Figure 39 shows 2 LTC6102s being used to measure the discharge and charge currents on a 12-cell battery stack. To achieve a large dynamic range while maintaining a high level of accuracy the LTC6102 is required. The circuit shown is able to accurately measure  $\pm 200$  Amps to 0.1 Amps. The offset of the LTC6102 will only contribute a 20mA error. To maintain a very low sleep current the  $V_{DRIVE}$  is used to disable the LTC6102 circuits so that they draw no current when the LTC6804 goes to sleep.

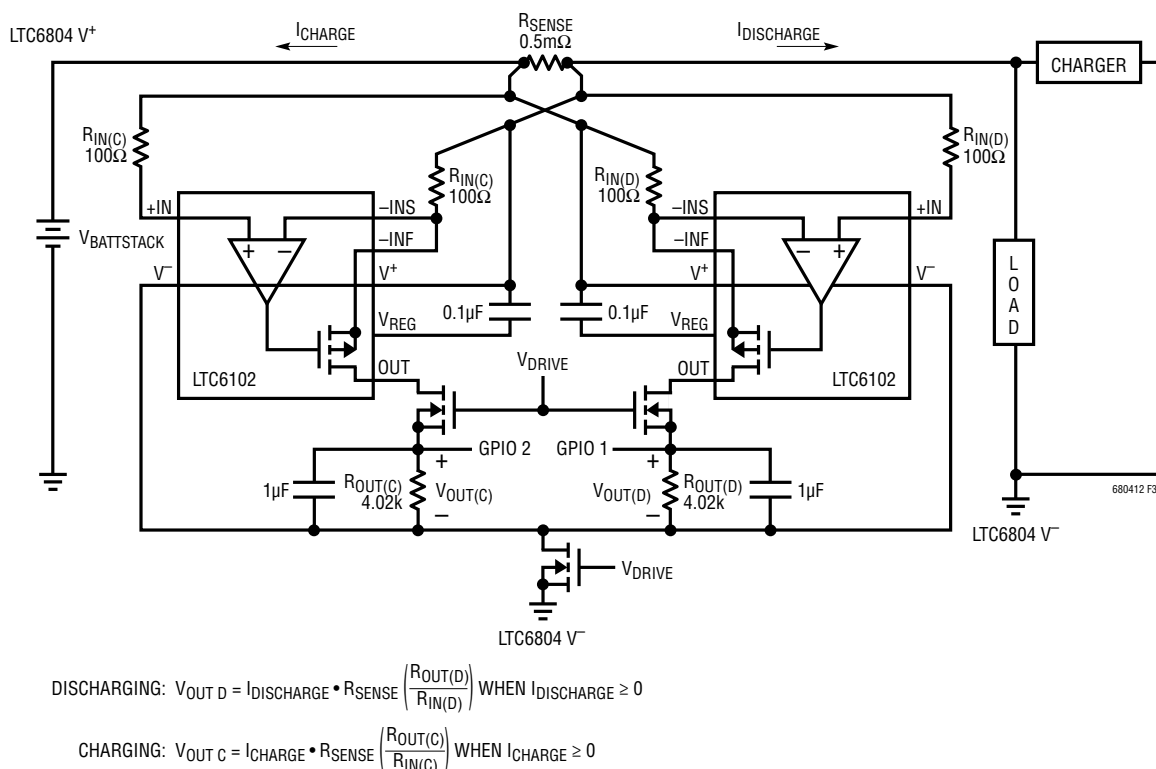


Figure 39. Monitoring Charge and Discharge Currents with a LTC6102

680412fc

## APPLICATIONS INFORMATION

### USING THE LTC6804 WITH LESS THAN 12 CELLS

If the LTC6804 is powered by the battery stack, the minimum number of cells that can be monitored by the LTC6804 is governed by the supply voltage requirements of the LTC6804.  $V^+$  must be at least 11V to properly bias the LTC6804. Figure 40 shows an example of the LTC6804 when used to monitor eight cells with best cell measurement synchronization. The 12 cells monitored by the LTC6804 are split into two groups of 6 cells and are measured using two internal multiplexers and two ADCs. To optimize measurement synchronization in applications with less than 12 Cells the unused C pins should be equally distributed between the top of the second mux (C12) and the top of the first mux (C6). If there are an odd number of cells being used, the top mux should have fewer cells connected. The unused cell channels should be tied to the other unused channels on the same mux and then connected to the battery stack through a 100 $\Omega$  resistor. The unused inputs will result in a reading of 0V for those cells channels. It is also acceptable to connect in the conventional sequence with all unused cell inputs at the top.

### isoSPI IBIAS and ICMP Setup

The LTC6804 allows the isoSPI links of each application to be optimized for power consumption or for noise immunity. The power and noise immunity of an isoSPI system is determined by the programmed  $I_B$  current, which controls the isoSPI signaling currents. Bias current  $I_B$  can range from 100 $\mu$ A to 1mA. Internal circuitry scales up this bias current to create the isoSPI signal currents equal to  $20 \cdot I_B$ . A low  $I_B$  reduces the isoSPI power consumption in the READY and ACTIVE states, while a high  $I_B$  increases the amplitude of the differential signal voltage  $V_A$  across the matching termination resistor,  $R_M$ . The  $I_B$  current is programmed by the sum of the  $R_{B1}$  and  $R_{B2}$  resistors connected between the 2V IBIAS pin and GND as shown in

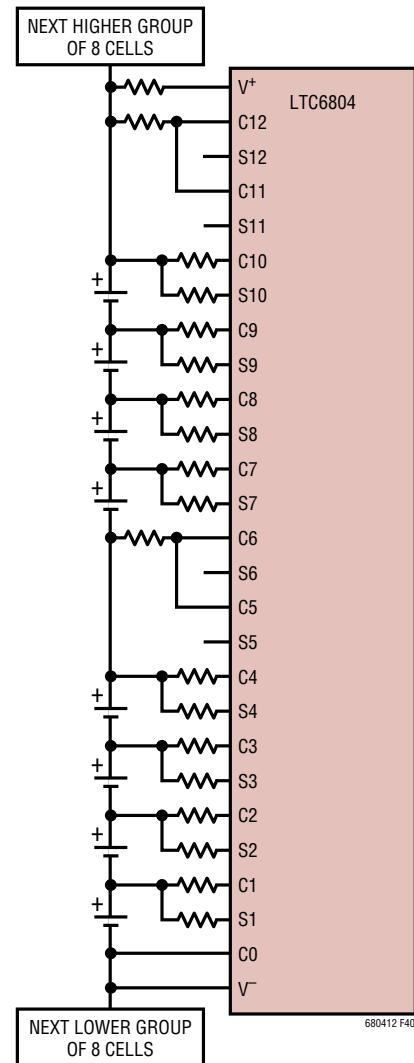
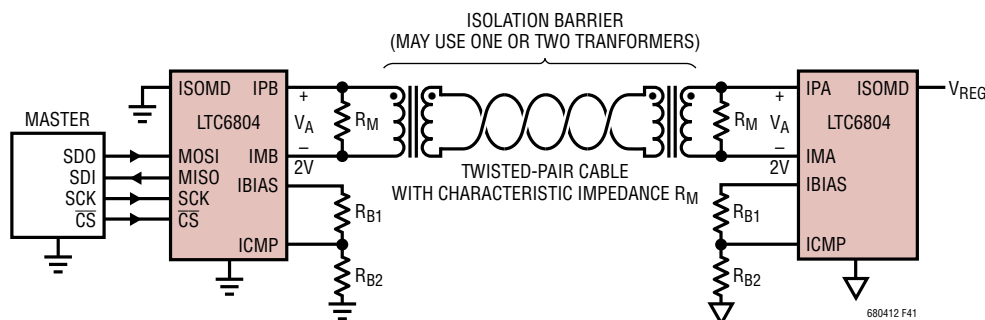


Figure 40. 8 Cell Connection Scheme

Figure 41. The receiver input threshold is set by the ICMP voltage that is programmed with the resistor divider created by the  $R_{B1}$  and  $R_{B2}$  resistors. The receiver threshold will be half of the voltage present on the ICMP pin.

## APPLICATIONS INFORMATION



### Figure 41. isoSPI Circuit

The following guidelines should be used when setting the bias current (100µA to 1mA)  $I_B$  and the receiver comparator threshold voltage  $V_{ICMP}/2$ :

$$R_M = \text{Transmission Line Characteristic Impedance } Z_0$$

Signal Amplitude  $V_A = (20 \cdot I_B) \cdot (R_M/2)$

$$V_{TCMP} \text{ (Receiver Comparator Threshold)} = K \cdot V_A$$

$$V_{ICMP} \text{ (voltage on ICMP pin)} = 2 \cdot V_{TCMP}$$

$$R_{B2} = V_{ICMP}/I_B$$

$$R_{B1} = (2/I_B) - R_{B2}$$

Select  $I_B$  and  $K$  (Signal Amplitude  $V_A$  to Receiver Comparator Threshold ratio) according to the application:

For lower power links:  $I_B = 0.5\text{mA}$  and  $K = 0.5$

For full power links:  $I_B = 1\text{mA}$  and  $K = 0.5$

For long links (>50m):  $I_B = 1\text{mA}$  and  $K = 0.25$

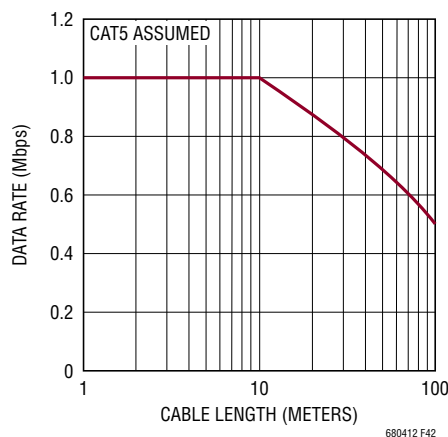
For addressable multi-drop:  $I_B = 1\text{mA}$  and  $K = 0.4$

For applications with little system noise, setting  $I_B$  to 0.5mA is a good compromise between power consumption and noise immunity. Using this  $I_B$  setting with a 1:1 transformer and  $R_M = 100\Omega$ ,  $R_{B1}$  should be set to 3.01k and  $R_{B2}$  set to 1k. With typical CAT5 twisted pair, these settings will allow for communication up to 50m. For applications in very noisy environments or that require cables longer than 50m it is recommended to increase  $I_B$  to 1mA. Higher drive current compensates for the increased insertion loss in the cable and provides high noise immunity. When using cables over 50m and a transformer with a 1:1 turns ratio and  $R_M = 100\Omega$ ,  $R_{B1}$  would be 1.5k and  $R_{B2}$  would be 499 $\Omega$ .

The maximum clock rate of an isoSPI link is determined by the length of the isoSPI cable. For cables 10 meters or less, the maximum 1MHz SPI clock frequency is possible. As the length of the cable increases, the maximum possible SPI clock rate decreases. This dependence is a result of the increased propagation delays that can create possible timing violations. Figure 42 shows how the maximum data rate reduces as the cable length increases when using a CAT5 twisted pair.

Cable delay affects three timing specifications:  $t_{CLK}$ ,  $t_6$  and  $t_7$ . In the Electrical Characteristics table, each of these specifications is de-rated by 100ns to allow for 50ns of cable delay. For longer cables, the minimum timing parameters may be calculated as shown below:

$$t_{CLK}, t_6 \text{ and } t_7 > 0.9\mu s + 2 \cdot t_{CABLE}(0.2m \text{ per ns})$$



### Figure 42. Data Rate vs Cable Length



## APPLICATIONS INFORMATION

### Implementing a Modular isoSPI Daisy Chain

The hardware design of a daisy-chain isoSPI bus is identical for each device in the network due to the daisy-chain point-to-point architecture. The simple design as shown in Figure 41 is functional, but inadequate for most designs. The termination resistor  $R_M$  should be split and bypassed with a capacitor as shown in Figure 43. This change provides both a differential and a common mode termination, and as such, increases the system noise immunity.

The use of cables between battery modules, particularly in automotive applications, can lead to increased noise susceptibility in the communication lines. For high levels of electromagnetic interference (EMC), additional filtering is recommended. The circuit example in Figure 43 shows the use of common mode chokes (CMC) to add common mode noise rejection from transients on the battery lines. The use of a center tapped transformer will also provide additional noise performance. A bypass capacitor connected to the center tap creates a low impedance for common mode noise (Figure 43b). Since transformers without a center tap can be less expensive, they may be preferred. In this case, the addition of a split termination resistor and a bypass capacitor (Figure 43a) can enhance the isoSPI performance. Large center tap capacitors greater than 10nF should be avoided as they may prevent the isoSPI common mode voltage from settling. Common mode chokes similar to those used in Ethernet or CANbus applications are recommended. Specific examples are provided in Table 49.

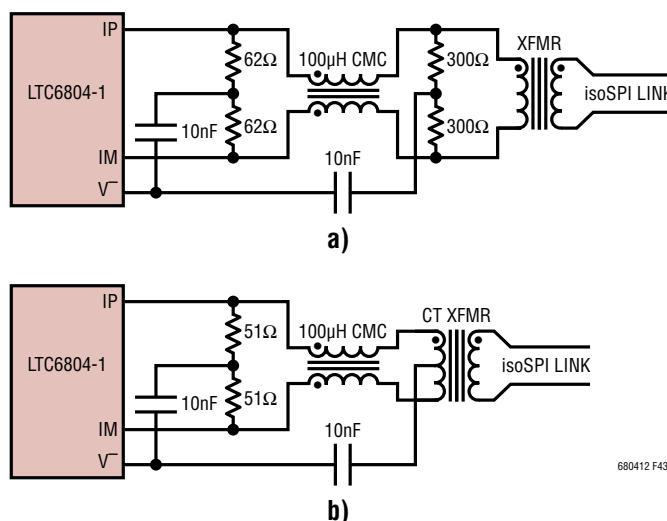


Figure 43. Daisy Chain Interface Components

An important daisy chain design consideration is the number of devices in the isoSPI network. The length of the chain determines the serial timing and affects data latency and throughput. The maximum number of devices in an isoSPI daisy chain is strictly dictated by the serial timing requirements. However, it is important to note that the serial read back time, and the increased current consumption, might dictate a practical limitation.

For a daisy chain, two timing considerations for proper operation dominate (see Figure 20):

1.  $t_6$ , the time between the last clock and the rising chip select, must be long enough.
2.  $t_5$ , the time from a rising chip select to the next falling chip select (between commands), must be long enough.

Both  $t_5$  and  $t_6$  must be lengthened as the number of LTC6804 devices in the daisy chain increases. The equations for these times are below:

$$t_5 > (\# \text{ devices} \cdot 70\text{ns}) + 900\text{ns}$$

$$t_6 > (\# \text{ devices} \cdot 70\text{ns}) + 950\text{ns}$$



## APPLICATIONS INFORMATION

### Connecting Multiple LTC6804-1s on the Same PCB

When connecting multiple LTC6804-1 devices on the same PCB, only a single transformer is required between the LTC6804-1 isoSPI ports. The absence of the cable also reduces the noise levels on the communication lines and often only a split termination is required. Figure 44 shows an example application that has multiple LTC6804-1s on the same PCB, communicating to the bottom MCU through an LTC6820 isoSPI driver. If a transformer with a center tap is used, a capacitor can be added for better noise rejection. Additional noise filtering can be provided with discrete common mode chokes (not shown) placed to both sides of the single transformer.

On single board designs with low noise requirements, it is possible for a simplified capacitor-isolated coupling as shown in Figure 45 to replace the transformer. Dual Zener diodes are used at each IC to clamp the common mode voltage to stay within the receiver's input range. The optional common mode choke (CMC) provides noise rejection with symmetrically tapped termination. The 590Ω resistor creates a resistor divider with the termination resistors and attenuates common mode noise. The 590Ω value is chosen to provide the most noise attenuation while maintaining sufficient differential signal. The circuit is designed such that  $I_B$  and  $V_{ICMP}$  are the same as would be used for a transformer based system with cables over 50m.

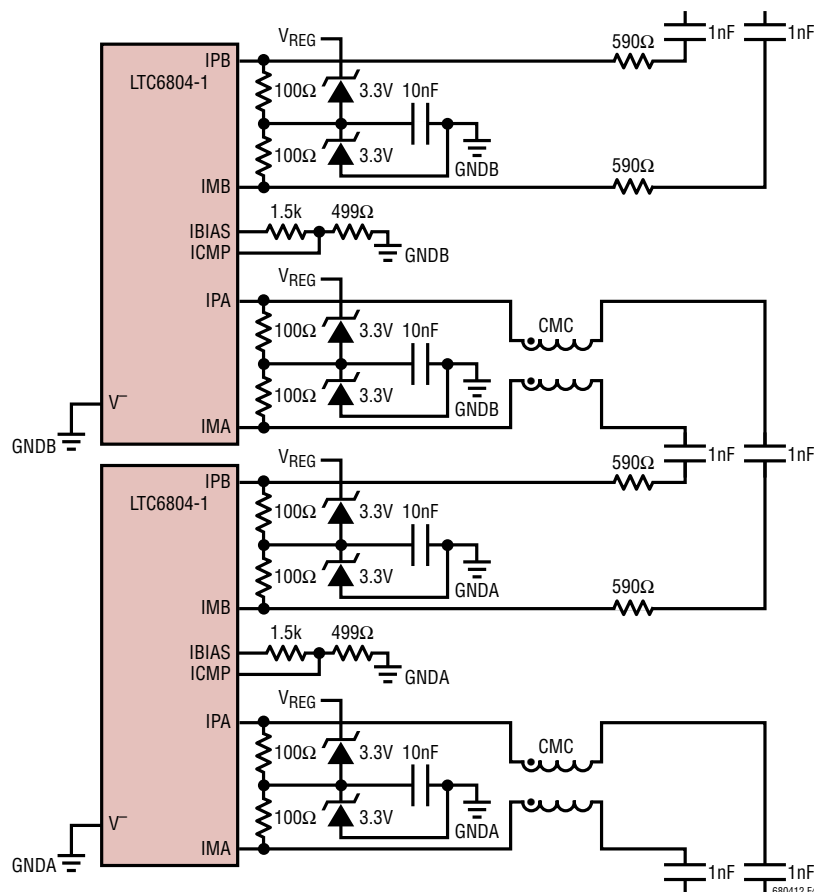


Figure 45. Capacitive Isolation Coupling for LTC6804-1s on the Same PCB

## APPLICATIONS INFORMATION

### Connecting an MCU to an LTC6804-1 with an isoSPI Data Link

The LTC6820 will convert standard 4-wire SPI into a 2-wire isoSPI link that can communicate directly with the LTC6804. An example is shown in Figure 46. The LTC6820 can be used in applications to provide isolation between the microcontroller and the stack of LTC6804s. The LTC6820 also enables system configurations that have the BMS controller at a remote location relative to the LTC6804 devices and the battery pack.

### Configuring the LTC6804-2 in a Multi-Drop isoSPI Link

The addressing feature of the LTC6804-2 allows multiple devices to be connected to a single isoSPI master by distributing them along one twisted pair, essentially creating a large parallel SPI network. A basic multi-drop system is shown in Figure 47; the twisted pair is terminated only at the beginning (master) and the end of the cable. In between, the additional LTC6804-2s are connected to short stubs on the twisted pair. These stubs should be kept short, with as little capacitance as possible, to avoid degrading the termination along the isoSPI wiring.

When an LTC6804-2 is not addressed, it will not transmit data pulses. This scheme eliminates the possibility for collisions since only the addressed device returns data to the master. Generally, multi-drop systems are best confined to compact assemblies where they can avoid excessive isoSPI pulse-distortion and EMC pickup.

### Basic Connection of the LTC6804-2 in a Multi-Drop Configuration

In a multi-drop isoSPI bus, placing the termination at the ends of the transmission line provides the best performance (with 100Ω typically). Each of the LTC6804 isoSPI ports should couple to the bus with a resistor network, as shown in Figure 48a. Here again, a center-tapped transformer offers the best performance and a common mode choke (CMC) increases the noise rejection further, as shown in Figure 48b. Figure 48b also shows the use of an RC snubber at the IC connections as a means to suppress resonances (the IC capacitance provides sufficient out-of-band rejection). When using a non-center-tapped transformer, a virtual CT can be generated by connecting a CMC as a voltage-splitter. Series resistors are recommended to decouple the LTC6804 and board parasitic capacitance from the transmission line. Reducing these parasitics on the transmission line will minimize reflections.

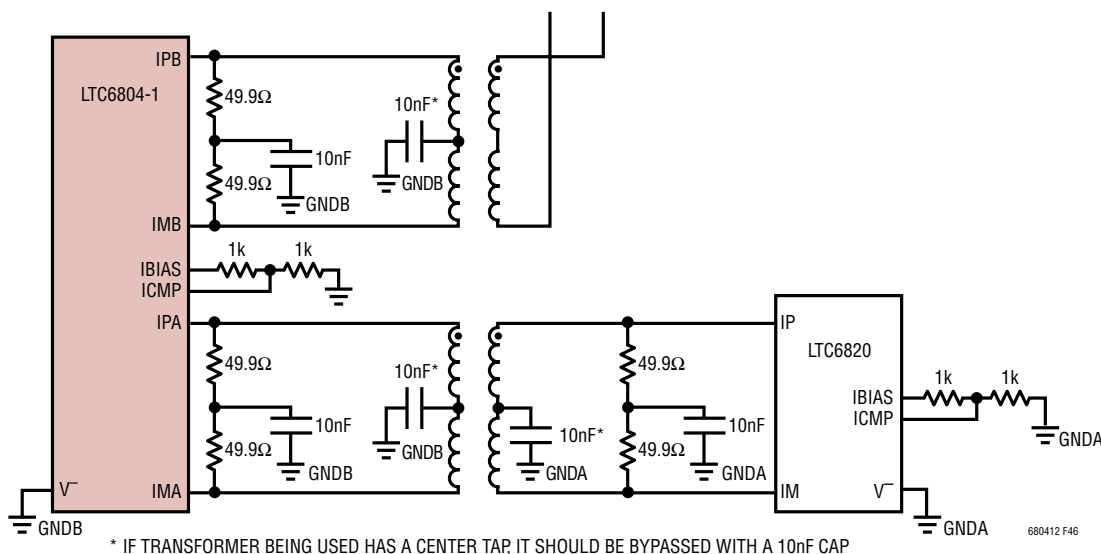


Figure 46. Interfacing an LTC6804-1 with a µC Using an LTC6820 for Isolated SPI Control

## APPLICATIONS INFORMATION

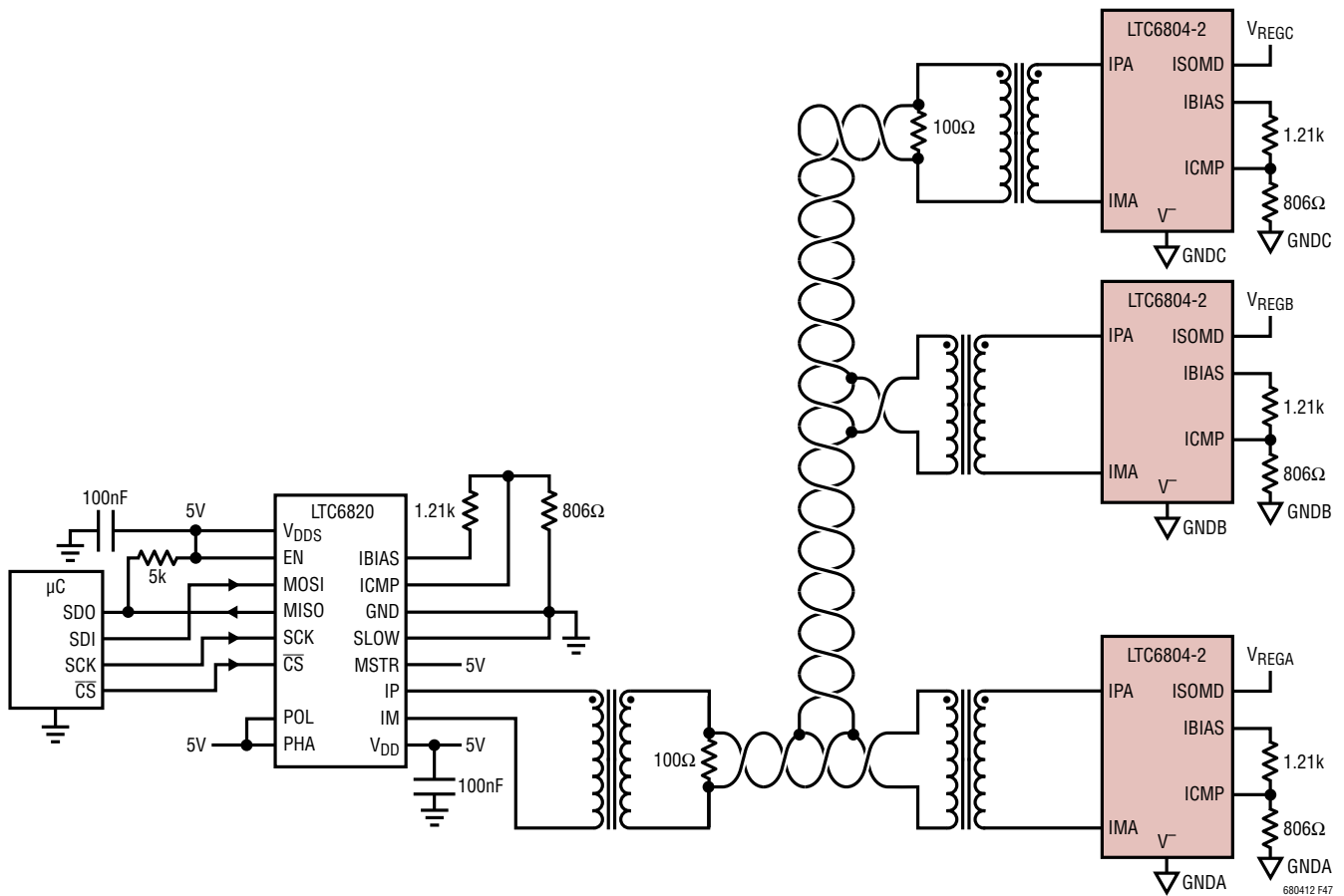


Figure 47. Connecting the LTC6804-2 in a Multi-Drop Configuration

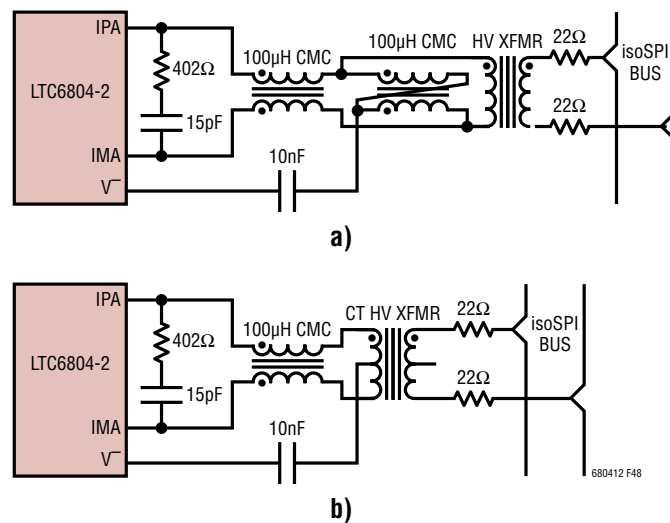


Figure 48. Preferred isoSPI Bus Couplings For Use With LTC6804-2

## APPLICATIONS INFORMATION

Table 48. Recommended Transformers

MANUFACTURER	PART NUMBER	TEMPERATURE RANGE	V <sub>WORKING</sub>	V <sub>HIPOT</sub> /60s	CT	CMC	H	L	W (W/LEADS)	PINS	AEC-Q200
<b>Dual Transformers</b>											
Pulse	HX1188FNL	–40°C to 85°C	60V (est)	1.5kVrms	●	●	6.0mm	12.7mm	9.7mm	16SMT	–
Pulse	HX0068ANL	–40°C to 85°C	60V (est)	1.5kVrms	●	●	2.1mm	12.7mm	9.7mm	16SMT	–
Pulse	HM2100NL	–40°C to 105°C	1000V	4.3kVdc	–	●	3.4mm	14.7mm	14.9mm	10SMT	●
Pulse	HM2102NL	–40°C to 125°C	1000V	4.3kVdc	●	●	4.9mm	14.8mm	14.7mm	12SMT	●
Sumida	CLP178–C20114	–40°C to 125°C	1000V (est)	3.75kVrms	●	●	9mm	17.5mm	15.1mm	12SMT	–
Sumida	CLP0612–C20115		600Vrms	3.75kVrms	●	–	5.7mm	12.7mm	9.4mm	16SMT	–
Würth Elektronik	7490140110	–40°C to 85°C	250Vrms	4kVrms	●	●	10.9mm	24.6mm	17.0mm	16SMT	–
Würth Elektronik	7490140111	0°C to 70°C	1000V (est)	4.5kVrms	●	–	8.4mm	17.1mm	15.2mm	12SMT	–
Würth Elektronik	749014018	0°C to 70°C	250Vrms	4kVrms	●	●	8.4mm	17.1mm	15.2mm	12SMT	–
Halo	TG110–AE050N5LF	–40°C to 85/125°C	60V (est)	1.5kVrms	●	●	6.4mm	12.7mm	9.5mm	16SMT	●
<b>Single Transformers</b>											
Pulse	PE-68386NL	–40°C to 130°C	60V (est)	1.5kVdc	–	–	2.5mm	6.7mm	8.6mm	6SMT	–
Pulse	HM2101NL	–40°C to 105°C	1000V	4.3kVdc	–	●	5.7mm	7.6mm	9.3mm	6SMT	●
Würth Elektronik	750340848	–40°C to 105°C	250V	3kVrms	–	–	2.2mm	4.4mm	9.1mm	4SMT	–
Halo	TGR04–6506V6LF	–40°C to 125°C	300V	3kVrms	●	–	10mm	9.5mm	12.1mm	6SMT	–
Halo	TGR04–A6506NA6NL	–40°C to 125°C	300V	3kVrms	●	–	9.4mm	8.9mm	12.1mm	6SMT	●
TDK	ALT4532V–201–T001	–40°C to 105°C	60V (est)	~1kV	●	–	2.9mm	3.2mm	4.5mm	6SMT	●
Halo	TDR04–A550ALLF	–40°C to 105°C	1000V	5kVrms	●	–	6.4mm	8.9mm	16.6mm	6TH	●
Sumida	CEEH96BNP–LTC6804/11	–40°C to 125°C	600V	2.5kVrms	–	–	7mm	9.2mm	12.0mm	4SMT	–
Sumida	CEP99NP–LTC6804	–40°C to 125°C	600V	2.5kVrms	●	–	10mm	9.2mm	12.0mm	8SMT	–
Sumida	ESMIT–4180/A	–40°C to 105°C	250Vrms	3kVrms	–	–	3.5mm	5.2mm	9.1mm	4SMT	●
TDK	VGT10/9EE–204S2P4	–40°C to 125°C	250V (est)	2.8kVrms	●	–	10.6mm	10.4mm	12.7mm	8SMT	–

## Transformer Selection Guide

As shown in Figure 41, a transformer or pair of transformers isolates the isoSPI signals between two isoSPI ports. The isoSPI signals have programmable pulse amplitudes up to 1.6V<sub>P-P</sub> and pulse widths of 50ns and 150ns. To be able to transmit these pulses with the necessary fidelity the system requires that the transformers have primary inductances above 60μH and a 1:1 turns ratio. It is also necessary to use a transformer with less than 2.5μH of leakage inductance. In terms of pulse shape the primary inductance will mostly effect the pulse droop of the 50ns and 150ns pulses. If the primary inductance is too low, the pulse amplitude will begin to droop and decay over the pulse period. When the pulse droop is severe enough, the effective pulse width seen by the receiver will drop substantially, reducing noise margin. Some droop is acceptable as long as it is a relatively small percentage of

the total pulse amplitude. The leakage inductance primarily affects the rise and fall times of the pulses. Slower rise and fall times will effectively reduce the pulse width. Pulse width is determined by the receiver as the time the signal is above the threshold set at the ICMP pin. Slow rise and fall times cut into the timing margins. Generally it is best to keep pulse edges as fast as possible. When evaluating transformers, it is also worth noting the parallel winding capacitance. While transformers have very good CMRR at low frequency, this rejection will degrade at higher frequencies, largely due to the winding to winding capacitance. When choosing a transformer, it is best to pick one with less parallel winding capacitance when possible.

When choosing a transformer, it is equally important to pick a part that has an adequate isolation rating for the application. The working voltage rating of a transformer is a key spec when selecting a part for an application.

Interconnecting daisy-chain links between LTC6804-1 devices see <60V stress in typical applications; ordinary pulse and LAN type transformers will suffice. Multi-drop connections and connections to the LTC6820, in general, may need much higher working voltage ratings for good long-term reliability. Usually, matching the working voltage to the voltage of the entire battery stack is conservative. Unfortunately, transformer vendors will often only specify one-second HV testing, and this is not equal to the long-term (“permanent”) rating of the part. For example, according to most safety standards a 1.5kV rated transformer is expected to handle 230V continuously, and a 3kV device is capable of 1100V long-term, though manufacturers may not always certify to those levels (refer to actual vendor data for specifics). Usually, the higher voltage transformers are called “high-isolation” or “reinforced insulation” types by the suppliers. Table 48 shows a list of transformers that have been evaluated in isoSPI links.

In most applications a common mode choke is also necessary for noise rejection. Table 49 includes a list of suitable CMCs if the CMC is not already integrated into the transformer being used.

**Table 49. Recommended Common Mode Chokes**

MANUFACTURER	PART NUMBER
TDK	ACT45B-101-2P
Murata	DLW43SH101XK2

### isoSPI Layout Guidelines

Layout of the isoSPI signal lines also plays a significant role in maximizing the noise immunity of a data link. The following layout guidelines are recommended:

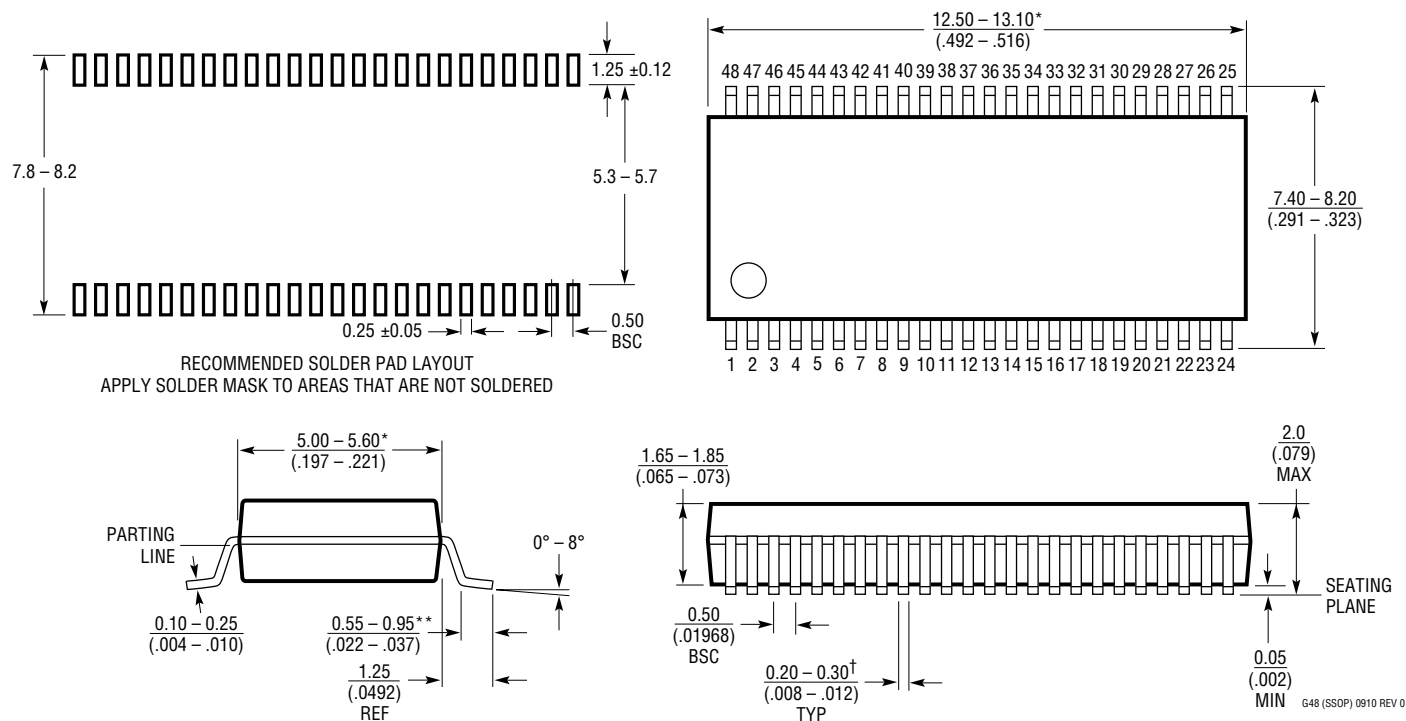
1. The transformer should be placed as close to the isoSPI cable connector as possible. The distance should be kept less than 2cm. The LTC6804 should be placed close to but at least 1cm to 2cm away from the transformer to help isolate the IC from magnetic field coupling.
2. A V<sup>-</sup> ground plane should not extend under the transformer, the isoSPI connector or in between the transformer and the connector.
3. The isoSPI signal traces should be as direct as possible while isolated from adjacent circuitry by ground metal or space. No traces should cross the isoSPI signal lines, unless separated by a ground plane on an inner layer.



## PACKAGE DESCRIPTION

Please refer to <http://www.linear.com/product/LTC6804-1#packaging> for the most recent package drawings.

### G Package 48-Lead Plastic SSOP (5.3mm) (Reference LTC DWG # 05-08-1887 Rev 0)



## REVISION HISTORY

REV	DATE	DESCRIPTION	PAGE NUMBER
A	10/13	T <sub>JMAX</sub> corrected from 125°C to 150°C	3
		WDT pin description updated	17, 30, 56, 57
		Information added to Recommended Transformers table	68
B	6/14	Correction to TME Test Conditions, V(CO) = V <sup>-</sup>	4, 5
		Description of T <sub>SLEEP</sub> added to STANDBY State Discussion	20
		Correction to Temperature Range for TMS Spec, 125°C instead of 85°C	22
		Note regarding potential differences between CO and V <sup>-</sup> added	27
		Correction to Measurement Range for Accuracy Check, 2.985V to 3.015V	27, 51
		Clarification of CLRSTAT command, which also clears RSVD bits	28
		Description of Reserved Bits Added	30, 51
		Clarification: Watchdog timer is reset by Qualified Wake-up Signal	30
		Clarification: SPI master supports only SPI mode 3	31
		Correction to data register, Dn[3:0] changed to Dn[7:0]	32
C	10/16	Discussion of Address, Broadcast and Polling Commands edited for Clarity	43-46
		Absolute maximum voltage between V <sup>+</sup> to C12 Added	2
		Note added in table to define I <sub>B</sub>	22
		Explanation added for issuing ADSTAT command with CHST = 100	27, 50
		Table 18 (read codes for I <sup>2</sup> C master operation) added	33
		Explanation of setting SPI strength using R <sub>B1</sub> and R <sub>B2</sub>	36
		Explanation of the SPI terminating resistor, R <sub>M</sub>	37
		Explanation of SPI termination and use of a single LTC6804	38
		Figure 18 added to single LTC6804 SPI termination	40
		Explanation of waking up the LTC6804 daisy chain	43
		Note added to Fully Isolated Power section to include a diode from V <sup>+</sup> to top of cell	59
		Section added for isoSPI IBIAS and ICMP setup	67, 68
		Section added for modular isoSPI daisy chain	69
		Section added for multiple LTC6804s on the same PCB	71
		Section added for connecting an MCU to an LTC6804-1	72
		Section added for configuring an LTC6804-2 multidrop	72
		Section added for basic connection of an LTC6804-2 multidrop	72
		Figure 47, 48 added to show isoSPI connections	73
		Section added for Transformer Selection Guide	74
		Section added for isoSPI Layout Guidelines	75

PART NUMBER	DESCRIPTION	COMMENTS
<a href="#">LTC6801</a>	Independent Multicell Battery Stack Fault Monitor	Monitors Up to 12 Series-Connected Battery Cells for Undervoltage or Overvoltage. Companion to <a href="#">LTC6802</a> , <a href="#">LTC6803</a> and <a href="#">LTC6804</a>
<a href="#">LTC6802</a>	Precision Multicell Battery Stack Monitor	1st Generation: Superseded by the <a href="#">LTC6804</a> and <a href="#">LTC6803</a> for New Designs
<a href="#">LTC6803</a>	Precision Multicell Battery Stack Monitor	2nd Generation: Functionally Enhanced and Pin Compatible to the <a href="#">LTC6802</a>
<a href="#">LTC6820</a>	Isolated Bidirectional Communications Interface for SPI	Provides an Isolated Interface for SPI Communication Up to 100 Meters, Using a Twisted Pair. Companion to the <a href="#">LTC6804</a>
<a href="#">LTC3300</a>	High Efficiency Bidirectional Multicell Battery Balancer	Bidirectional Synchronous Flyback Balancing of Up to 6 Li-Ion or LiFeP04 Cells in Series. Up to 10A Balancing Current (Set by External Components). Bidirectional Architecture Minimizes Balancing Time and Power Dissipation. Up to 92% Charge Transfer Efficiency. 48-Lead Exposed Pad QFN and LQFP Packages

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