

## Description

The DIODES™ AP62800 is an 8A, synchronous buck converter with a wide input voltage range of 4.5V to 17V. The device fully integrates a 22mΩ high-side power MOSFET and a 10mΩ low-side power MOSFET to provide high-efficiency step-down DC-DC conversion.

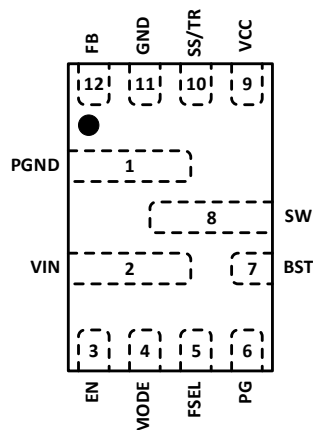
The AP62800 device is easily used by minimizing the external component count due to its adoption of Constant On-Time (COT) control to achieve fast transient response, easy loop stabilization, and low output voltage ripple.

The AP62800 design is optimized for Electromagnetic Interference (EMI) reduction. The device has a proprietary gate driver scheme to resist switching node ringing without sacrificing MOSFET turn-on and turn-off times, which reduces high-frequency radiated EMI noise caused by MOSFET switching.

The device is available in a V-QFN2030-12 (Type A) package.

## Pin Assignments

V-QFN2030-12 (Type A)



Top View

## Features

- VIN: 4.5V to 17V
- Output Voltage (VOUT): 0.6V to 7V
- 8A Continuous Output Current
- 0.6V ± 1% Reference Voltage
- 195μA Quiescent Current
- Selectable Switching Frequency
  - 400kHz
  - 800kHz
  - 1.2MHz
- Selectable Operation Modes
  - Pulse Frequency Modulation (PFM)
  - Ultrasonic Mode (USM)
  - Pulse Width Modulation (PWM)
- Programmable Soft-Start Time
- Proprietary Gate Driver Design for Best EMI Reduction
- Power-Good Indicator with 5MΩ Internal Pull-up Resistor
- Precision Enable Threshold to Adjust UVLO
- Protection Circuitry
  - Undervoltage Lockout (UVLO)
  - Cycle-by-Cycle Valley Current Limit
  - Thermal Shutdown
- Totally Lead-Free & Fully RoHS Compliant (Notes 1 & 2)**
- Halogen and Antimony Free. "Green" Device (Note 3)**
- For automotive applications requiring specific change control (i.e. parts qualified to AEC-Q100/101/104/200, PPAP capable, and manufactured in IATF 16949 certified facilities), please [contact us](https://www.diodes.com/quality/product-definitions/) or your local Diodes representative.**

<https://www.diodes.com/quality/product-definitions/>

## Applications

- 5V and 12V distributed power bus supplies
- Television sets and monitors
- White goods and small home appliances
- FPGA, DSP, and ASIC supplies
- Home audios
- Network systems
- Gaming consoles
- Consumer electronics
- General purpose point of loads

Notes:

1. No purposely added lead. Fully EU Directive 2002/95/EC (RoHS), 2011/65/EU (RoHS 2) & 2015/863/EU (RoHS 3) compliant.
2. See <https://www.diodes.com/quality/lead-free/> for more information about Diodes Incorporated's definitions of Halogen- and Antimony-free, "Green" and Lead-free.
3. Halogen- and Antimony-free "Green" products are defined as those which contain <900ppm bromine, <900ppm chlorine (<1500ppm total Br + Cl) and <1000ppm antimony compounds.

## Typical Application Circuit

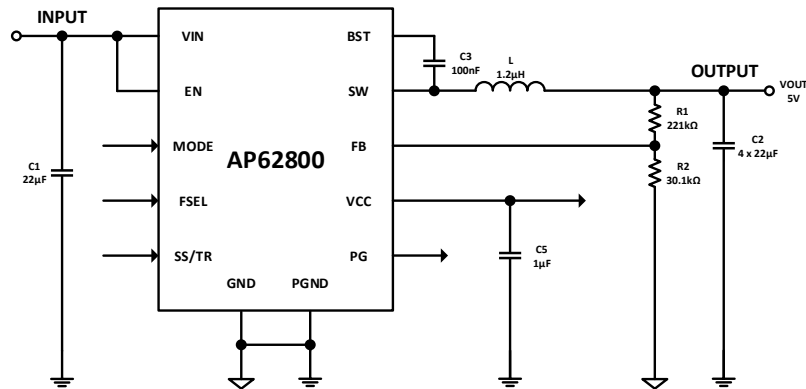


Figure 1. Typical Application Circuit

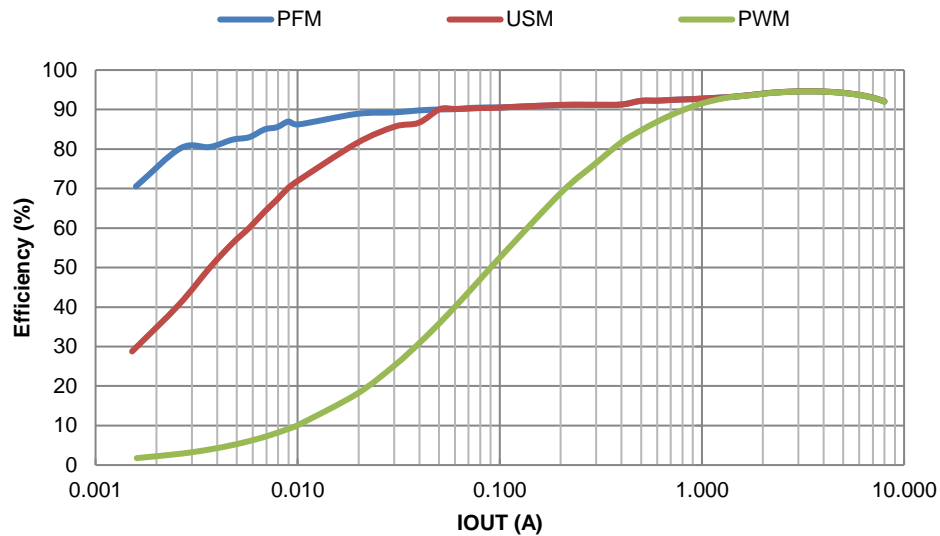


Figure 2. Efficiency vs. Output Current, VIN = 12V, VOUT = 5V, L = 1.2μH, fsw = 800kHz

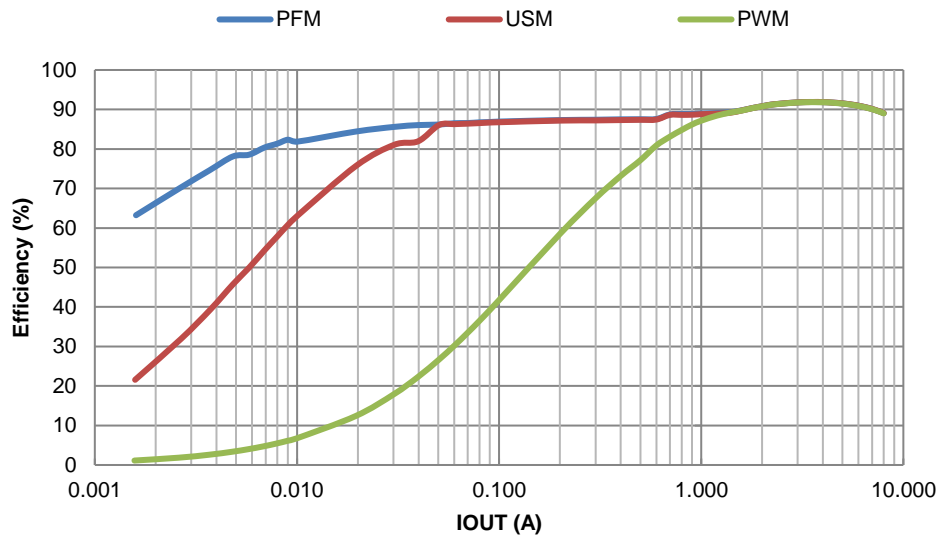


Figure 3. Efficiency vs. Output Current, VIN = 12V, VOUT = 3.3V, L = 1.0μH, fsw = 800kHz

## Pin Descriptions

Pin Name	Pin Number	Function
PGND	1	Power Ground. PGND must be connected to a single point ground and to as large a PGND plane as possible on the PCB for proper operation and optimized thermal performance.
VIN	2	Power Input. VIN supplies the power to the IC as well as the step-down converter power MOSFETs. Drive VIN with a 4.5V to 17V power source. Bypass VIN to GND with a suitably large capacitor to eliminate noise due to the switching of the IC. See <b>Input Capacitor</b> section for more details.
EN	3	Enable Input. EN is a digital input that turns the regulator on or off. Drive EN high to turn on the regulator and low to turn it off. It can be left open for automatic startup. The EN has a precision threshold of 1.18V for programing the UVLO. See <b>Enable</b> section for more details.
MODE	4	MODE Select. MODE is used to select the operation mode of the device. Connect MODE to GND to program the device to operate in PFM Mode. Leave MODE floating to program the device to operate in USM. Connect MODE to VCC to program the device to operate in PWM Only Mode.
FSEL	5	Frequency Select. FSEL is used to select the switching frequency of the device. Connect FSEL to GND to program the switching frequency to 400kHz. Leave FSEL floating to program the switching frequency to 800kHz. Connect FSEL to VCC to program the switching frequency to 1.2MHz.
PG	6	Power-Good. PG is an open-drain output that is pulled to GND when the output voltage is out of its regulation limits or during soft-start. Connect an external pull-up resistor from PG to VCC.
BST	7	High-Side Gate Drive Boost Input. BST supplies the drive voltage for the high-side N-Channel power MOSFET. A 100nF capacitor is recommended from BST to SW to power the high-side driver.
SW	8	Power Switching Output. SW is the switching node that supplies power to the output. Connect the output LC filter from SW to the output load.
VCC	9	Internal Power Supply. VCC supplies the internal logic circuitry as well as the gate drivers. Connect a 1μF capacitor as close as possible to VCC and PGND. This pin is not active when EN is low.
SS/TR	10	Soft-Start and Tracking. SS/TR controls the soft-start, tracking, and sequencing of the output. Connect a ceramic capacitor from SS/TR to GND to program the soft-start time. Leave SS/TR floating to use the internal soft-start. See <b>Soft-Start, Tracking, and Sequencing</b> section for more details.
GND	11	Ground. GND is the main power ground for the control logic circuitry. It must have a Kelvin Connection to PGND.
FB	12	Feedback. FB is the sensing terminal for the output voltage. Connect this pin to the resistive divider of the output. See <b>Setting the Output Voltage</b> section for more details.

The schematic diagram illustrates the internal and external components of the LT8602 buck converter. The IC pins are numbered 1 through 12. Key components and connections include:

- Pin 1 (PGND):** Connected to ground.
- Pin 2 (VIN):** Connected to the input voltage source.
- Pin 3 (EN):** Enabled pin, connected to a 20kΩ resistor and a 1.2V reference.
- Pin 4 (MODE):** Mode select pin, connected to the Mode Select block.
- Pin 5 (FSEL):** Frequency select pin, connected to the On-Time Compute block.
- Pin 6 (PG):** Power good pin, connected to a 5MΩ resistor and ground.
- Pin 7 (BST):** Bootstrap pin, connected to the BST diode.
- Pin 8 (SW):** Switching node, connected to the SW node.
- Pin 9 (VCC):** Connected to the VCC regulator output.
- Pin 10 (SS/TR):** Sense/sense pin, connected to the SS/TR node.
- Pin 11 (GND):** Connected to ground.
- Pin 12 (FB):** Feedback pin, connected to the FB node.

Internal blocks and components shown in the schematic include:

- VCC Regulator:** A voltage regulator block that provides a stable VCC supply.
- Internal Reference:** A 0.6V reference voltage source.
- UVLO:** Under-voltage lockout block.
- OCP:** Over-current protection block.
- Control Logic:** The central logic block that coordinates the converter's operation.
- One-Shot:** A timing block used for the on-time.
- On-Time Compute:** A block that calculates the on-time based on feedback and frequency select.
- Minimum Off-Time:** A block that ensures a minimum off-time for the switching transistors.
- Thermal Shutdown:** A block that protects the IC from overheating.
- Mode Select:** A block that selects the operating mode based on the MODE pin.

External components and connections include:

- Resistors:** 20kΩ (EN), 5MΩ (PG), and various sense resistors (I<sub>1</sub>, I<sub>2</sub>, I<sub>SS</sub>).
- Capacitors:** Input filter capacitor, output filter capacitor, and bootstrap capacitor.
- Diodes:** BST diode, SW diode, and PG diode.
- Transistors:** Q1 (NMOS), Q2 (PMOS), and the internal reference diode.

### Figure 4. Functional Block Diagram

## Absolute Maximum Ratings (Note 4) (@ T<sub>A</sub> = +25°C, unless otherwise specified.)

Symbol	Parameter	Rating	Unit
V <sub>IN</sub>	Supply Pin Voltage	-0.3 to +19.0 (DC) -0.3 to 21.0 (400ms)	V
V <sub>CC</sub>	VCC Pin Voltage	-0.3 to +6.0	V
V <sub>EN</sub>	Enable/UVLO Pin Voltage	-0.3 to +19.0	V
V <sub>MODE</sub>	MODE Select Pin Voltage	-0.3 to +6.0	V
V <sub>FSEL</sub>	Frequency Select Pin Voltage	-0.3 to +6.0	V
V <sub>PG</sub>	Power-Good Pin Voltage	-0.3 to +6.0	V
V <sub>BST</sub>	Bootstrap Pin Voltage	V <sub>sw</sub> - 0.3 to V <sub>sw</sub> + 6.0	V
V <sub>SW</sub>	Switch Pin Voltage	-1.0 to V <sub>IN</sub> + 0.3 (DC) -2.5 to V <sub>IN</sub> + 2.0 (20ns)	V
V <sub>SS/TR</sub>	Soft-Start/Tracking Pin Voltage	-0.3 to +6.0	V
V <sub>FB</sub>	Feedback Pin Voltage	-0.3 to +6.0	V
T <sub>ST</sub>	Storage Temperature	-65 to +150	°C
T <sub>J</sub>	Junction Temperature	+160	°C
T <sub>L</sub>	Lead Temperature	+260	°C
<b>ESD Susceptibility (Note 5)</b>			
HBM	Human Body Model	±4000	V
CDM	Charged Device Model	±1000	V

Notes: 4. Stresses greater than those listed under *Absolute Maximum Ratings* can cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions* is not implied. Exposure to *Absolute Maximum Ratings* for extended periods can affect device reliability.  
5. Semiconductor devices are ESD sensitive and may be damaged by exposure to ESD events. Suitable ESD precautions should be taken when handling and transporting these devices.

## Thermal Resistance (Note 6)

Symbol	Parameter	Rating	Unit
θ <sub>JA</sub>	Junction to Ambient	V-QFN2030-12 (Type A) 40	°C/W
θ <sub>JC</sub>	Junction to Case	V-QFN2030-12 (Type A) 5.5	°C/W

Note: 6. Test condition for V-QFN2030-12 (Type A): Device mounted on FR-4 substrate, four-layer PCB, 2oz copper, with minimum recommended pad layout.

## Recommended Operating Conditions (Note 7) (@ T<sub>A</sub> = +25°C, unless otherwise specified.)

Symbol	Parameter	Min	Max	Unit
V <sub>IN</sub>	Supply Voltage	4.5	17.0	V
V <sub>OUT</sub>	Output Voltage	0.6	7.0	V
T <sub>A</sub>	Operating Ambient Temperature	-40	+85	°C
T <sub>J</sub>	Operating Junction Temperature	-40	+125	°C

Note: 7. The device function is not guaranteed outside of the recommended operating conditions.

**Electrical Characteristics** (@  $T_J = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ , unless otherwise specified. Min/Max limits apply across the recommended junction temperature range,  $-40^\circ\text{C}$  to  $+125^\circ\text{C}$ , and input voltage range, 4.5V to 17V, unless otherwise specified.)

Symbol	Parameter	Conditions	Min	Typ	Max	Unit
ISHDN	Shutdown Supply Current	$V_{EN} = 0\text{V}$	—	1	—	$\mu\text{A}$
I <sub>Q</sub>	Quiescent Supply Current	$V_{FB} = 0.85\text{V}$	—	195	—	$\mu\text{A}$
POR	VIN Power-on Reset Rising Threshold	—	4.0	4.25	4.45	V
UVLO	VIN Undervoltage Lockout Falling Threshold	—	—	3.95	—	V
VCC	VCC Output Voltage	$6.0\text{V} < V_{IN} < 17\text{V}$ $0 < I_{VCC} < 5\text{mA}$	4.75	5.0	5.25	V
I <sub>VCC</sub>	VCC Current Source	$V_{IN} = 6\text{V}$ , $V_{CC} = 0\text{V}$	—	30	—	mA
R <sub>DS(ON)1</sub>	High-Side Power MOSFET On-Resistance (Note 8)	—	—	22	—	m $\Omega$
R <sub>DS(ON)2</sub>	Low-Side Power MOSFET On-Resistance (Note 8)	—	—	10	—	m $\Omega$
I <sub>VALLEY_LIMIT</sub>	LS Valley Current Limit (Note 8)	From Source to Drain	9.5	10.5	11.8	A
INCL	LS Negative Current Limit	From Drain to Source	—	3.0	—	A
f <sub>sw</sub>	Oscillator Frequency	$V_{FSEL} = \text{GND}$ , $V_{OUT} = 5\text{V}$ CCM	—	400	—	kHz
		$V_{FSEL} = \text{Floating}$ , $V_{OUT} = 5\text{V}$ CCM	—	800	—	kHz
		$V_{FSEL} = V_{CC}$ , $V_{OUT} = 5\text{V}$ CCM	—	1200	—	kHz
V <sub>MODE_PFM</sub>	PFM Mode Logic Threshold	$V_{MODE} = \text{GND}$ , $V_{CC} = 5\text{V}$	—	—	0.7	V
V <sub>MODE_USM</sub>	Ultrasonic Mode Logic Threshold	$V_{MODE} = \text{Floating}$	—	2.5	—	V
V <sub>MODE_PWM</sub>	PWM Mode Logic Threshold	$V_{MODE} = V_{CC} = 5\text{V}$	4.2	—	—	V
t <sub>ON_MIN</sub>	Minimum On-Time	—	—	70	—	ns
t <sub>OFF_MIN</sub>	Minimum Off-Time	—	—	255	—	ns
V <sub>FB</sub>	Feedback Voltage	CCM	0.594	0.600	0.606	V
V <sub>EN_H</sub>	EN Logic High Threshold	—	—	1.20	1.25	V
V <sub>EN_L</sub>	EN Logic Low Threshold	—	1.03	1.12	—	V
I <sub>EN</sub>	EN Input Current	$V_{EN} = 1.5\text{V}$	—	5.1	—	$\mu\text{A}$
		$V_{EN} = 1\text{V}$	1.0	1.4	2.0	$\mu\text{A}$
t <sub>SS</sub>	Soft-Start Time	$V_{SS/TR} = \text{Floating}$	—	1	—	ms
I <sub>SS</sub>	Soft-Start Current Source	$V_{SS/TR} = 1.2\text{V}$	—	5	—	$\mu\text{A}$
PG <sub>UV_FALL</sub>	Undervoltage Falling Threshold	Percent of Output Regulation, Fault	—	85	—	%
PG <sub>UV_RISE</sub>	Undervoltage Rising Threshold	Percent of Output Regulation, Good	—	95	—	%
PG <sub>OV_RISE</sub>	Overvoltage Rising Threshold	Percent of Output Regulation, Fault	—	115	—	%
PG <sub>OV_FALL</sub>	Overvoltage Falling Threshold	Percent of Output Regulation, Good	—	105	—	%
t <sub>PG_RD</sub>	Power-Good Rise Delay Time	—	—	0.5	—	ms
V <sub>PG_OL</sub>	Power-Good Output Logic Low	$I_{PG} = -3\text{mA}$	—	—	0.4	V
R <sub>PG</sub>	Internal PG Pull-up Resistor	—	—	5	—	M $\Omega$
T <sub>SD</sub>	Thermal Shutdown (Note 8)	—	—	+160	—	$^\circ\text{C}$
T <sub>HYS</sub>	Thermal Shutdown Hysteresis (Note 8)	—	—	+30	—	$^\circ\text{C}$

Note: 8. Compliance to the datasheet limits is assured by one or more methods: production test, characterization, and/or design.

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.)

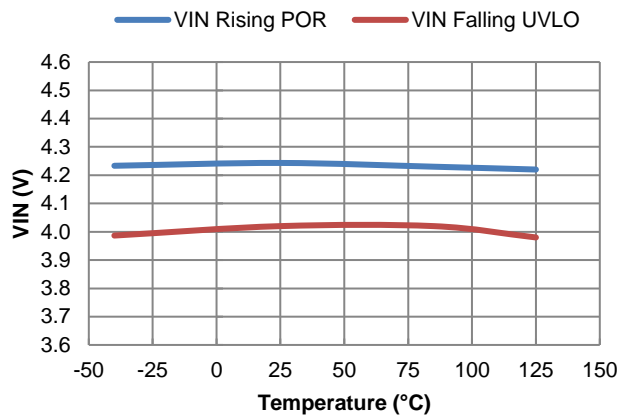


Figure 5. VIN Power-On Reset and UVLO vs. Temperature

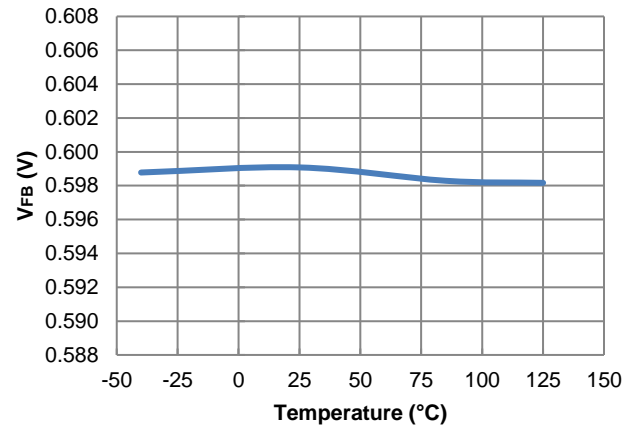


Figure 6.  $V_{FB}$  vs. Temperature

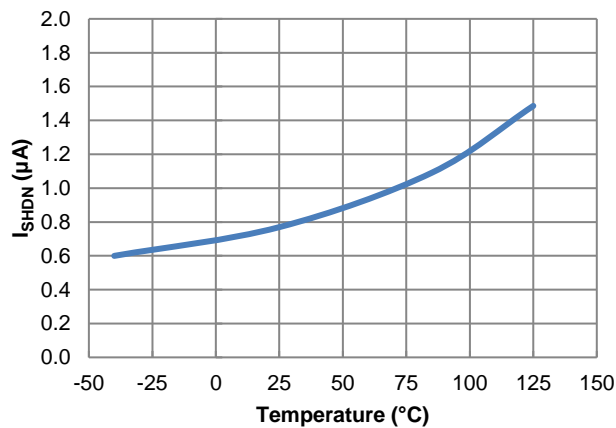


Figure 7.  $I_{SHDN}$  vs. Temperature

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.) (continued)

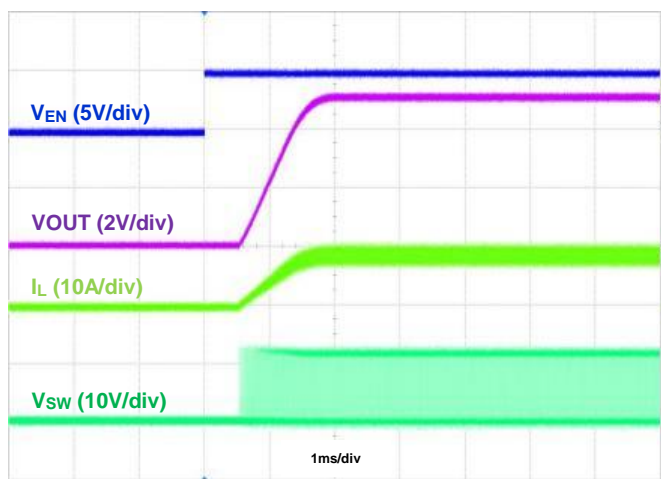


Figure 8. Startup Using EN, Showing Vsw, IOUT = 8A

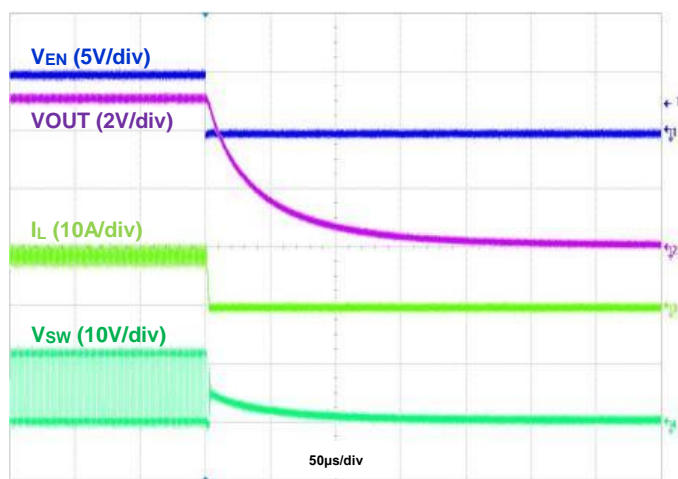


Figure 9. Shutdown Using EN, Showing Vsw, IOUT = 8A

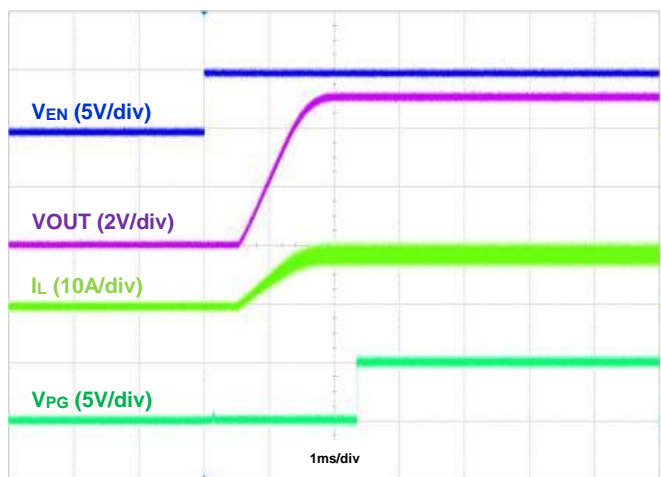


Figure 10. Startup Using EN, Showing VPG, IOUT = 8A

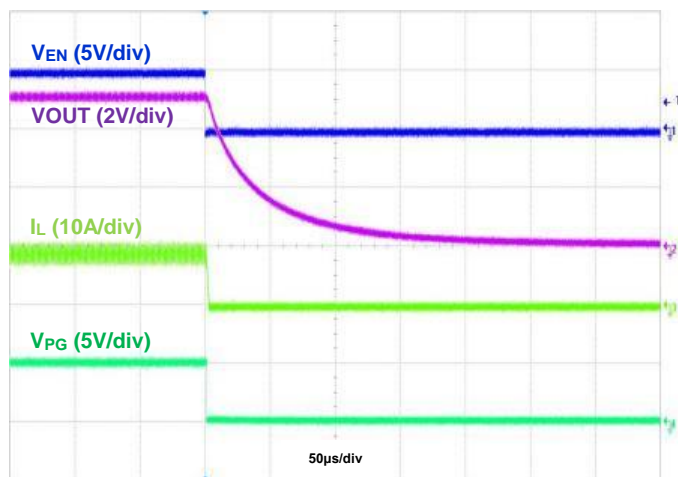


Figure 11. Shutdown Using EN, Showing VPG, IOUT = 8A

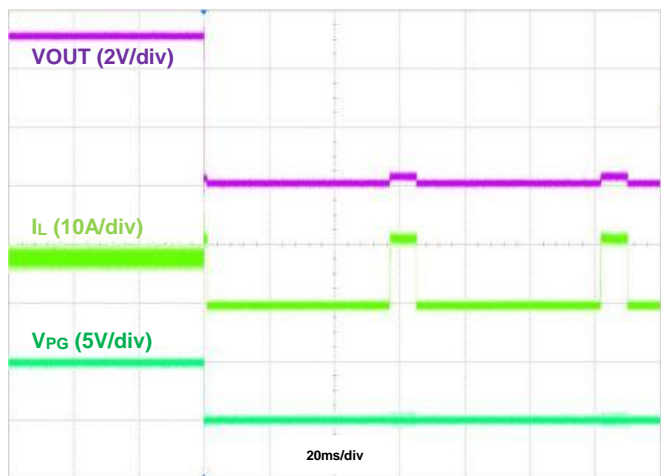


Figure 12. Output Short Protection, IOUT = 8A

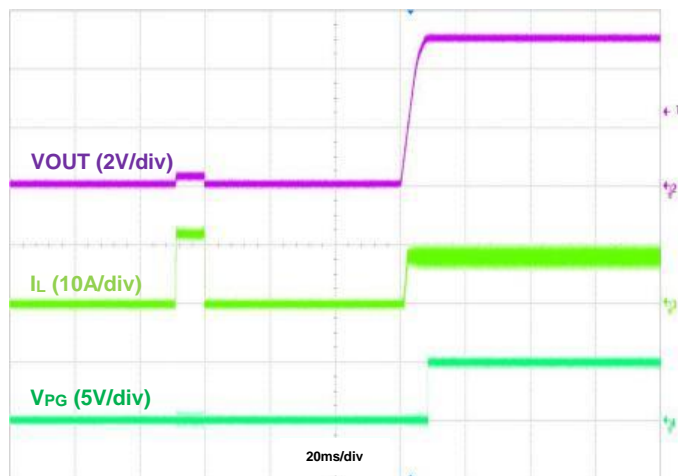


Figure 13. Output Short Recovery, IOUT = 8A



**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , MODE = GND (PFM), FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.)

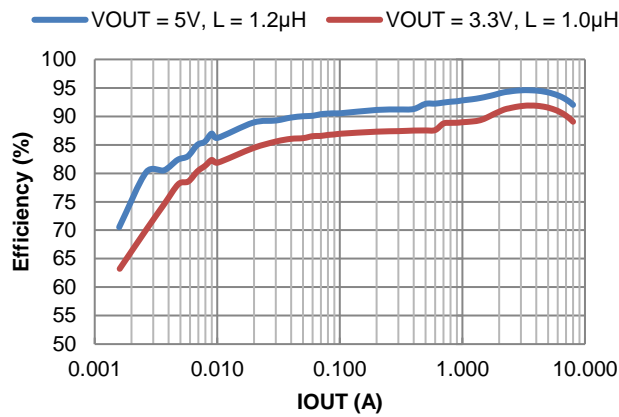


Figure 14. Efficiency vs. Output Current

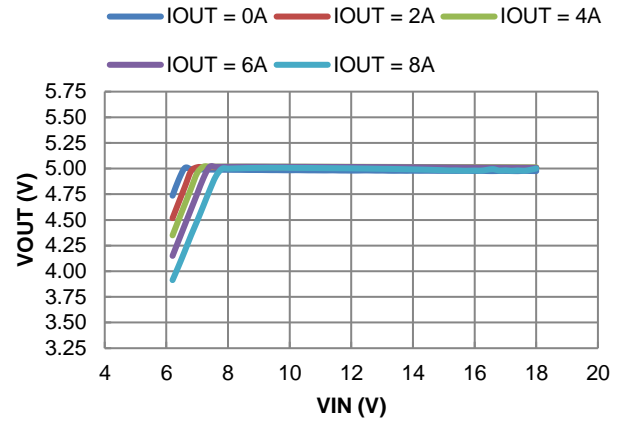


Figure 15. Line Regulation

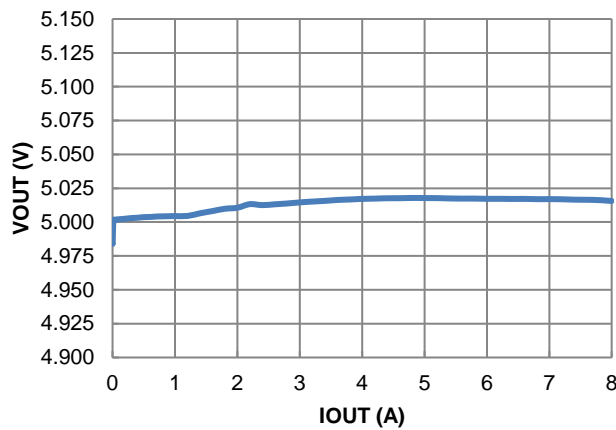


Figure 16. Load Regulation

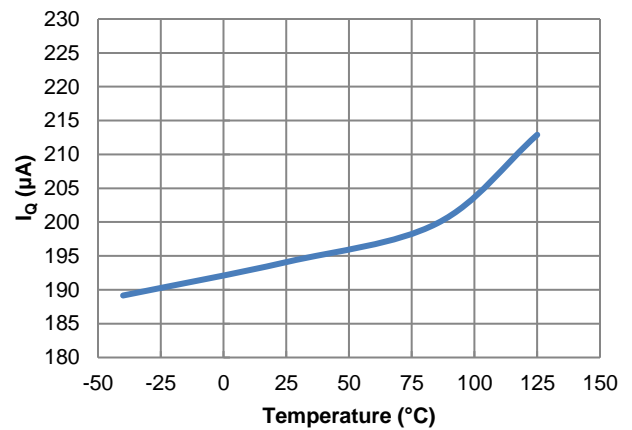


Figure 17.  $I_Q$  vs. Temperature

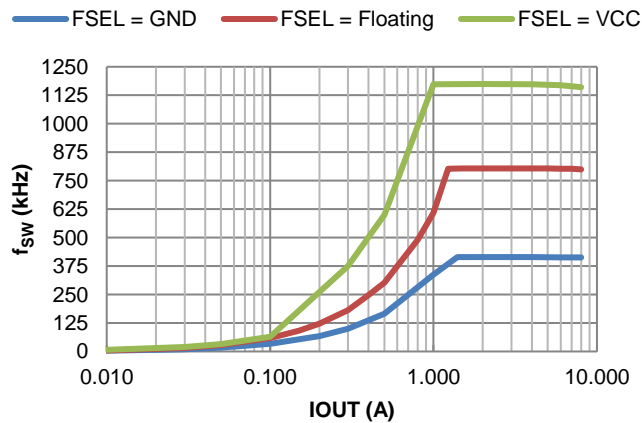


Figure 18.  $f_{sw}$  vs. Load

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ ,  $\text{MODE} = \text{GND (PFM)}$ ,  $\text{FSEL} = \text{Floating (f}_{\text{sw}} = 800\text{kHz)}$ ,  $\text{SS/TR} = \text{Floating (t}_{\text{ss}} = 1\text{ms)}$ ,  $\text{BOM} = \text{Table 1}$ , unless otherwise specified.) (continued)

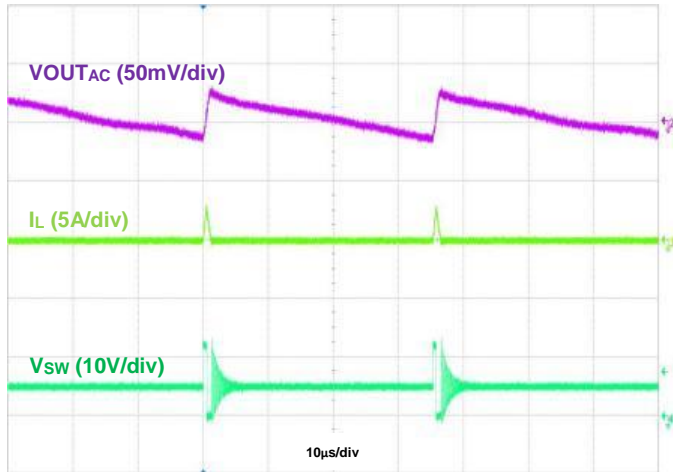


Figure 19. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 50\text{mA}$

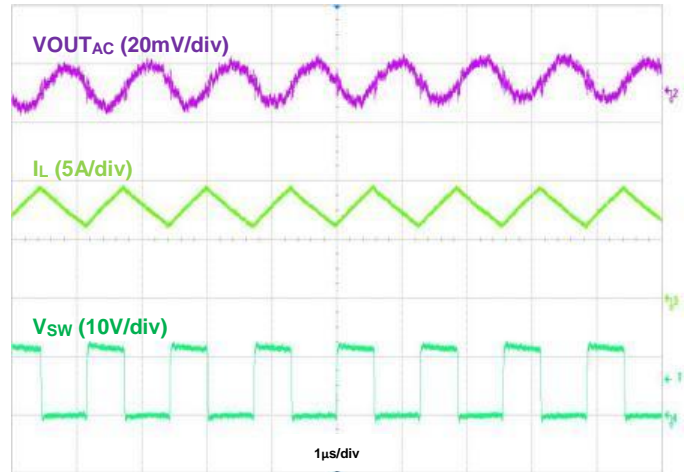


Figure 20. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 8\text{A}$

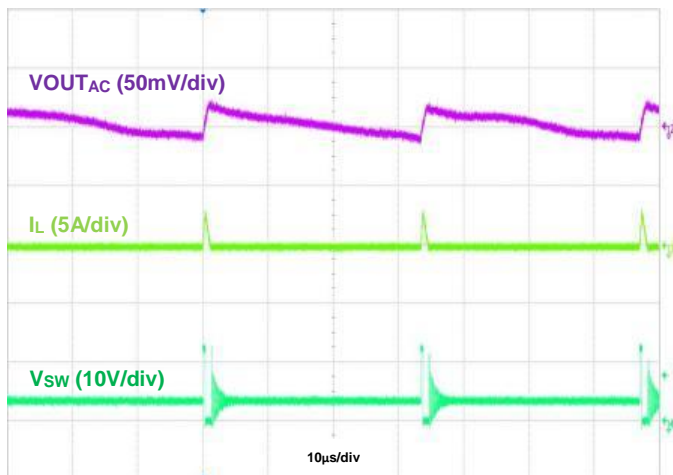


Figure 21. Output Voltage Ripple,  $V_{OUT} = 3.3\text{V}$ ,  $I_{OUT} = 50\text{mA}$

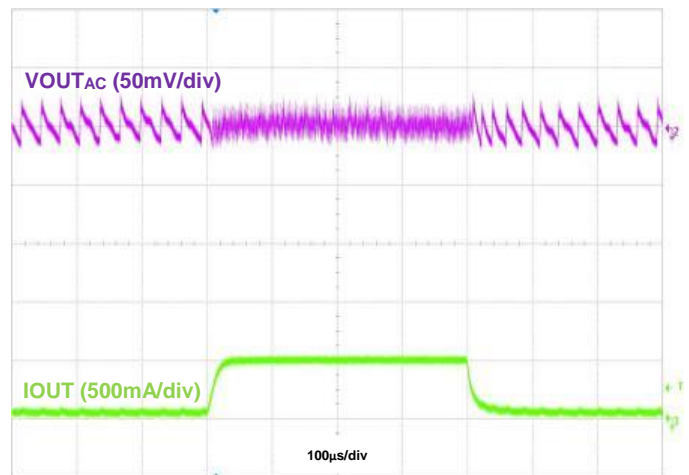


Figure 22. Load Transient,  $I_{OUT} = 50\text{mA}$  to  $500\text{mA}$  to  $50\text{mA}$

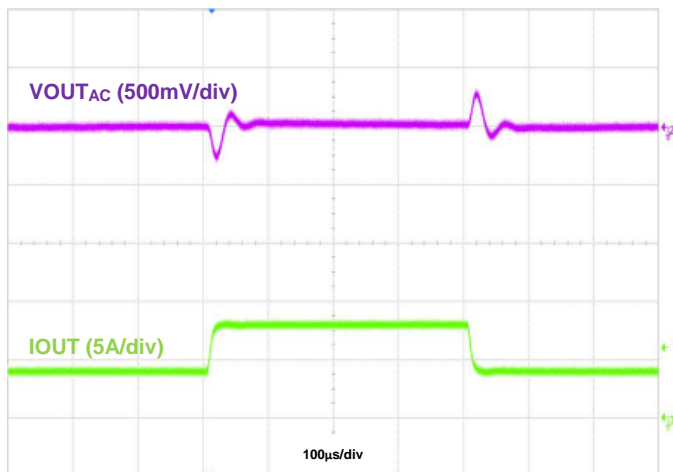


Figure 23. Load Transient,  $I_{OUT} = 4\text{A}$  to  $8\text{A}$  to  $4\text{A}$

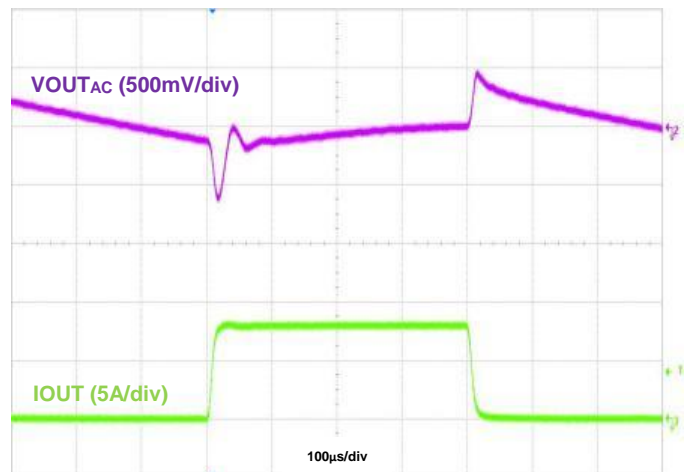


Figure 24. Load Transient,  $I_{OUT} = 50\text{mA}$  to  $8\text{A}$  to  $50\text{mA}$

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , MODE = Floating (USM), FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.)

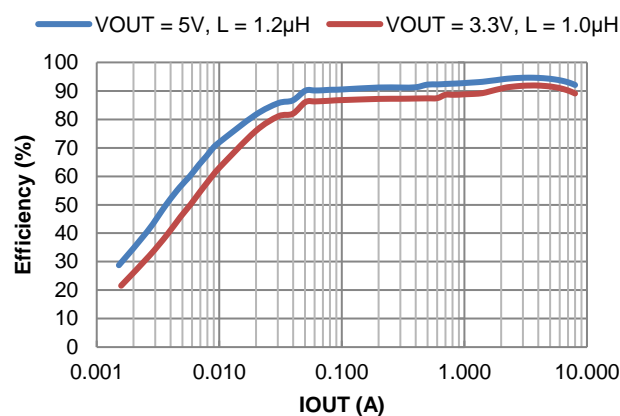


Figure 25. Efficiency vs. Output Current

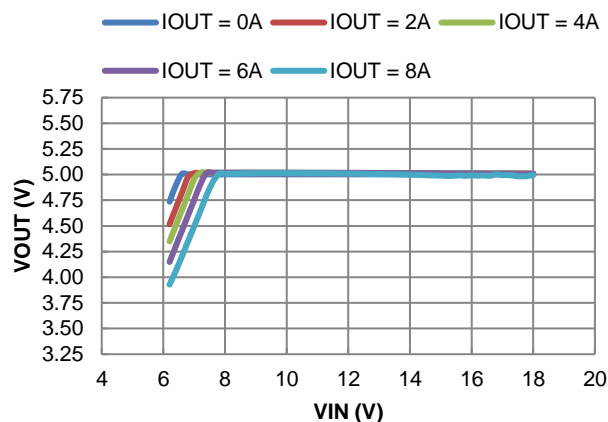


Figure 26. Line Regulation

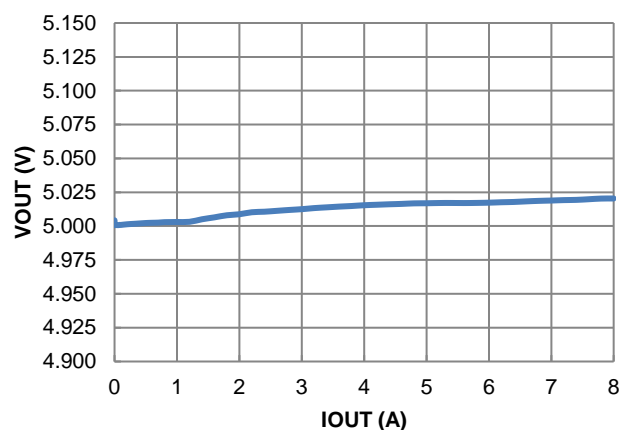


Figure 27. Load Regulation

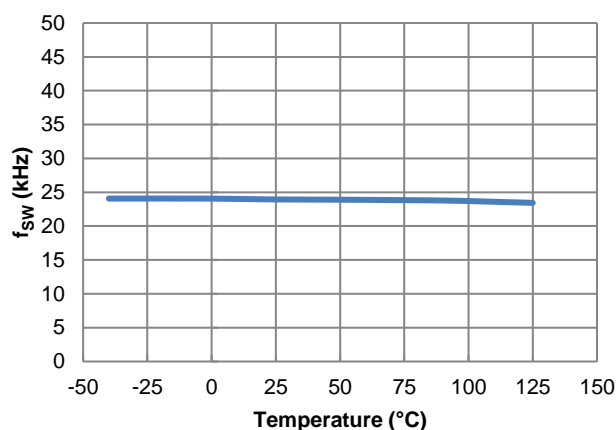


Figure 28.  $f_{sw}$  vs. Temperature,  $I_{OUT} = 0\text{A}$

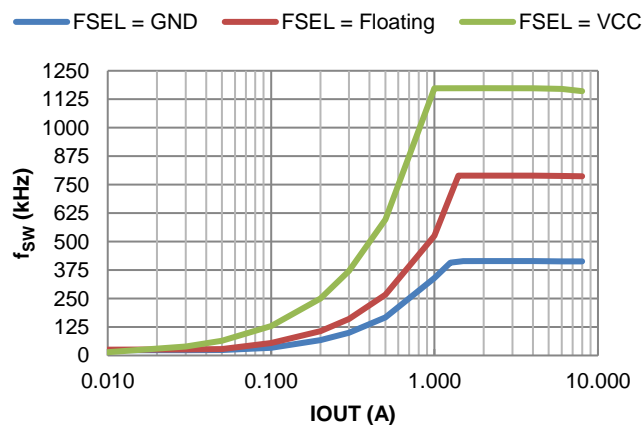


Figure 29.  $f_{sw}$  vs. Load

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , MODE = Floating (USM), FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.) (continued)

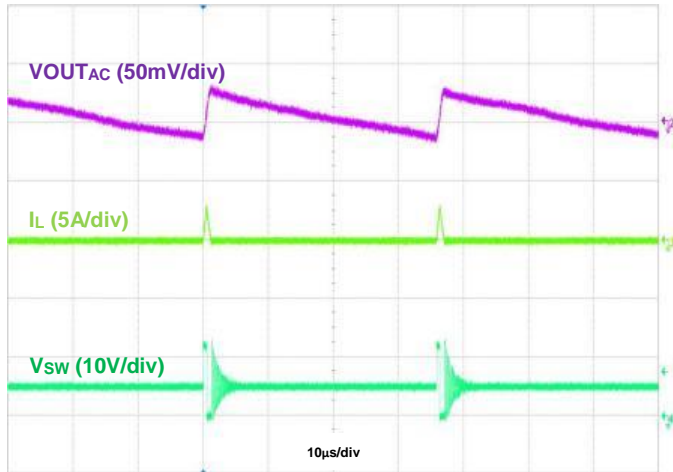


Figure 30. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 50\text{mA}$

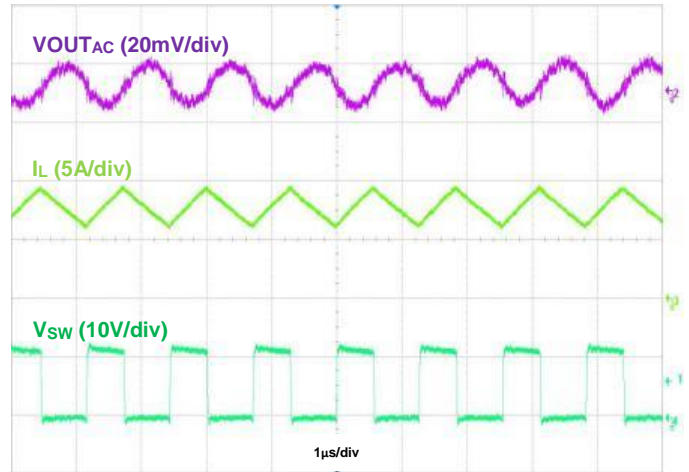


Figure 31. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 8\text{A}$

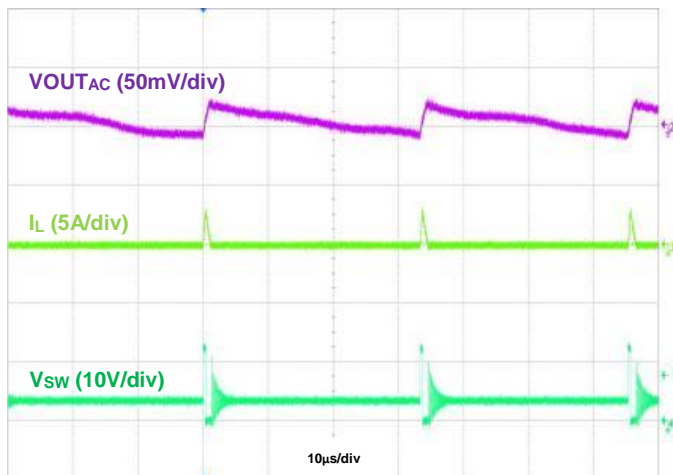


Figure 32. Output Voltage Ripple,  $V_{OUT} = 3.3\text{V}$ ,  $I_{OUT} = 50\text{mA}$

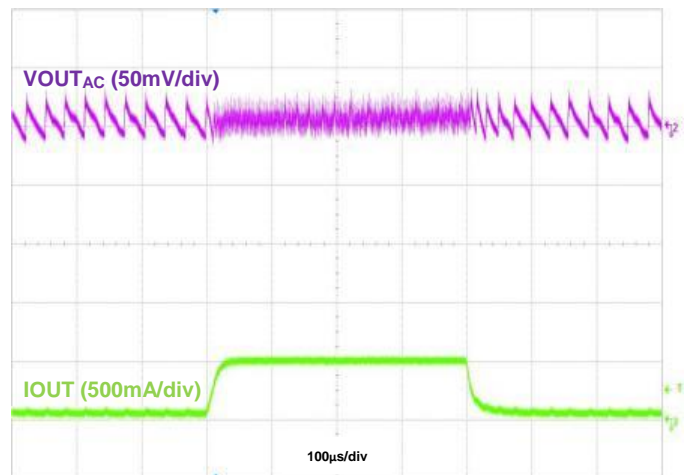


Figure 33. Load Transient,  $I_{OUT} = 50\text{mA}$  to 500mA to 50mA

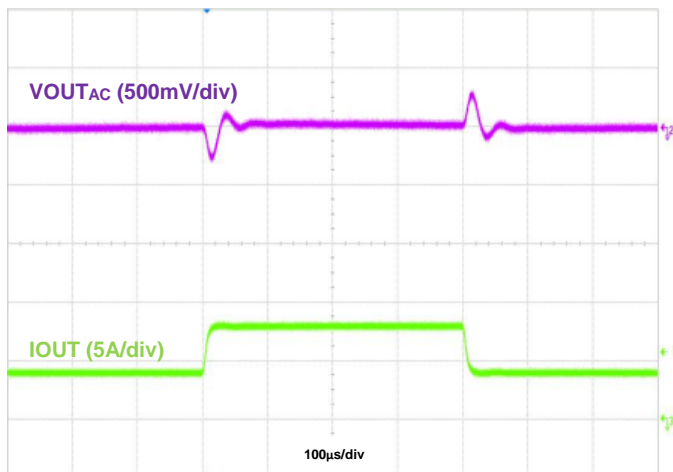


Figure 34. Load Transient,  $I_{OUT} = 4\text{A}$  to 8A to 4A

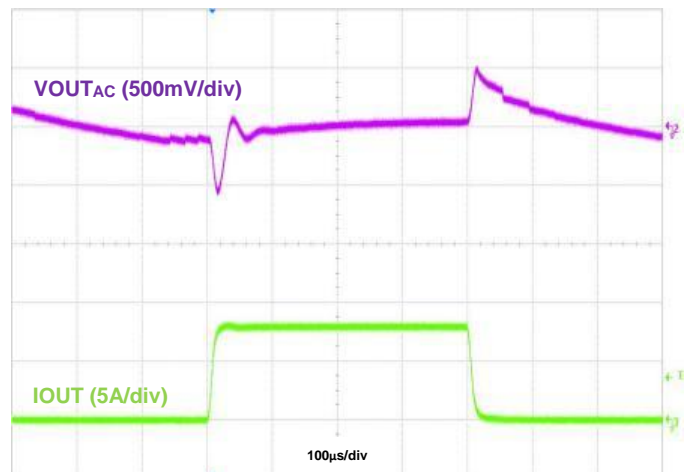


Figure 35. Load Transient,  $I_{OUT} = 50\text{mA}$  to 8A to 50mA

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ , MODE = VCC (PWM), FSEL = Floating ( $f_{sw} = 800\text{kHz}$ ), SS/TR = Floating ( $t_{ss} = 1\text{ms}$ ), BOM = Table 1, unless otherwise specified.)

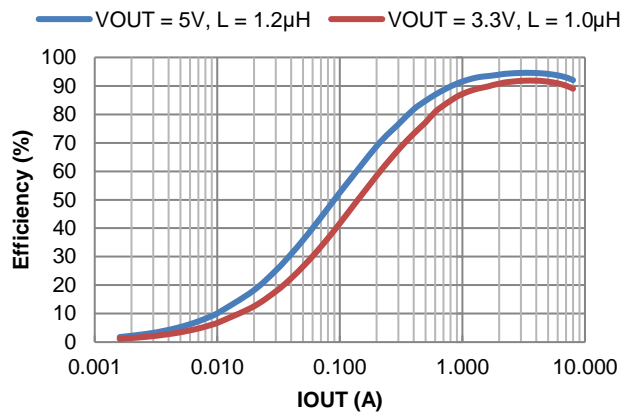


Figure 36. Efficiency vs. Output Current

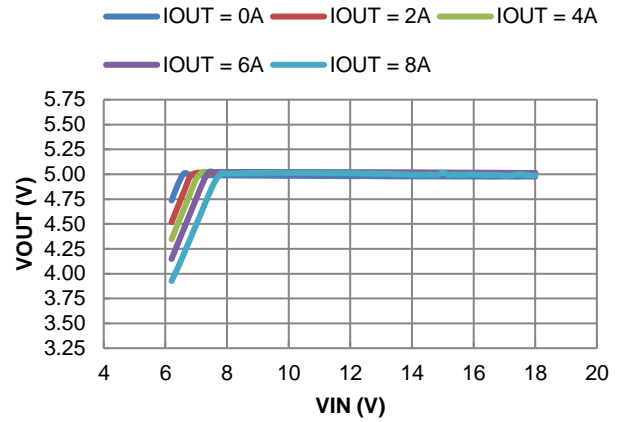


Figure 37. Line Regulation

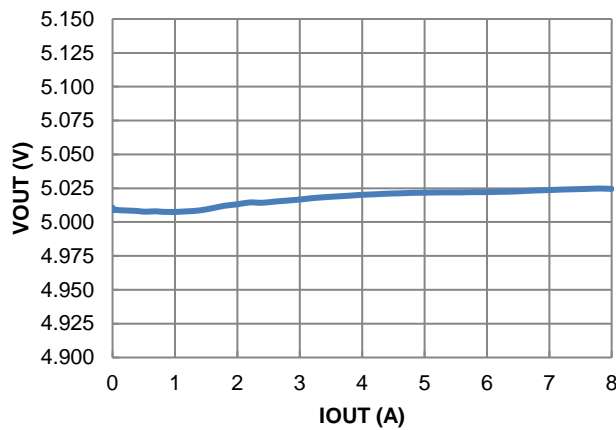


Figure 38. Load Regulation

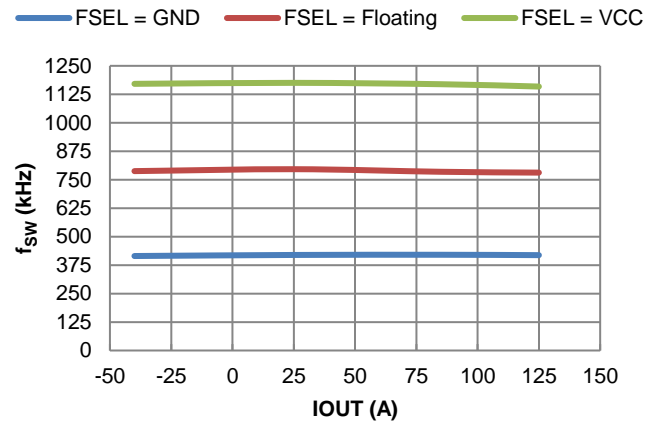


Figure 39.  $f_{sw}$  vs. Temperature,  $I_{OUT} = 0\text{A}$

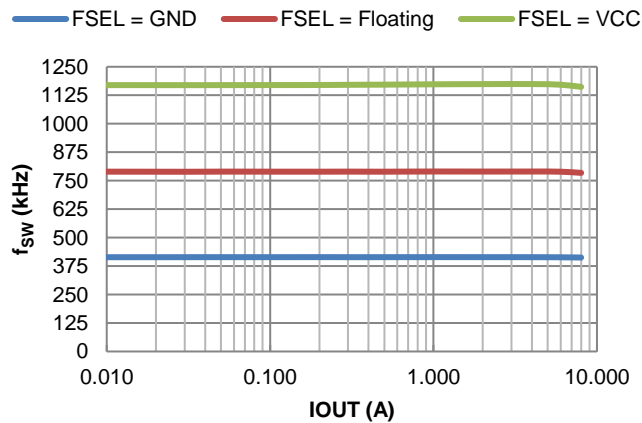


Figure 40.  $f_{sw}$  vs. Load

**Typical Performance Characteristics** (AP62800 @  $T_A = +25^\circ\text{C}$ ,  $V_{IN} = 12\text{V}$ ,  $V_{OUT} = 5\text{V}$ ,  $\text{MODE} = \text{VCC (PWM)}$ ,  $\text{FSEL} = \text{Floating (}f_{\text{sw}} = 800\text{kHz)}$ ,  $\text{SS/TR} = \text{Floating (}t_{\text{ss}} = 1\text{ms)}$ ,  $\text{BOM} = \text{Table 1}$ , unless otherwise specified.) (continued)

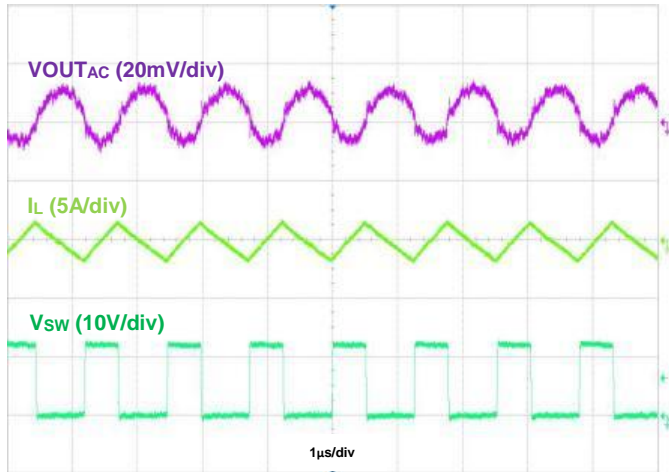


Figure 41. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 50\text{mA}$

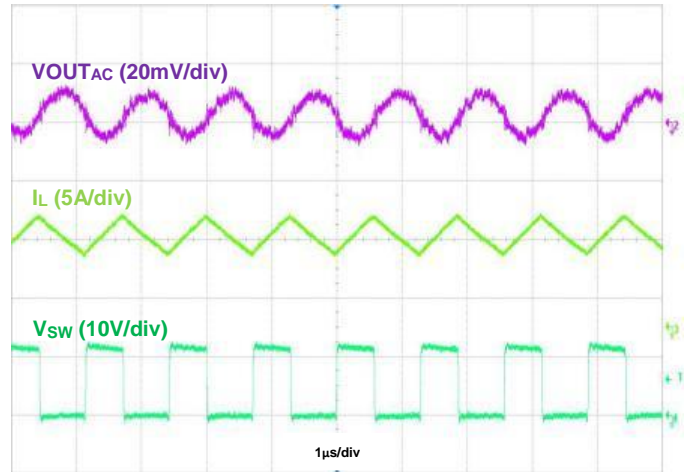


Figure 42. Output Voltage Ripple,  $V_{OUT} = 5\text{V}$ ,  $I_{OUT} = 8\text{A}$

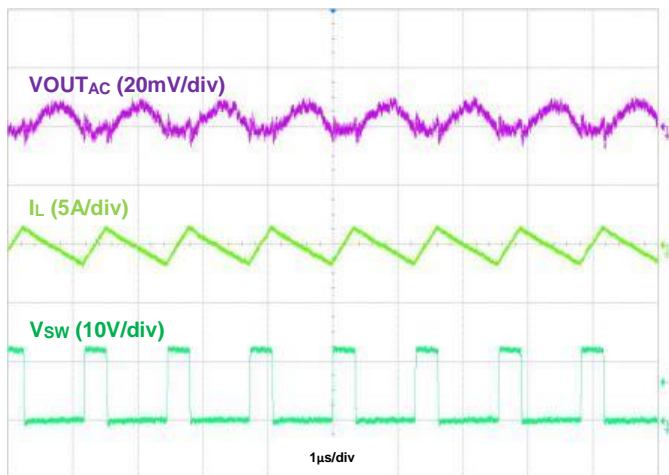


Figure 43. Output Voltage Ripple,  $V_{OUT} = 3.3\text{V}$ ,  $I_{OUT} = 50\text{mA}$

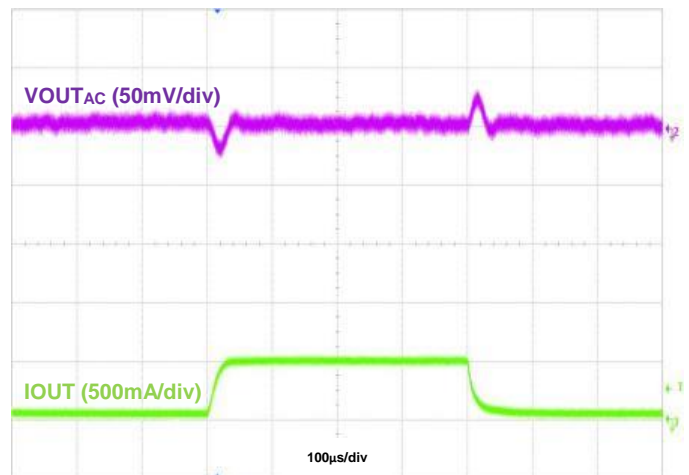


Figure 44. Load Transient,  $I_{OUT} = 50\text{mA}$  to  $500\text{mA}$  to  $50\text{mA}$

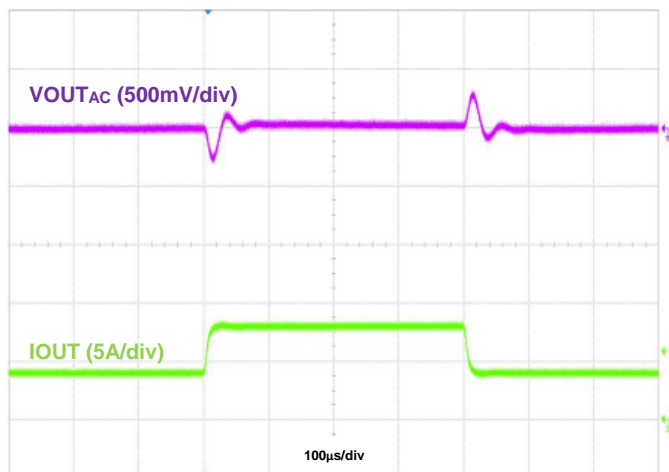


Figure 45. Load Transient,  $I_{OUT} = 4\text{A}$  to  $8\text{A}$  to  $4\text{A}$

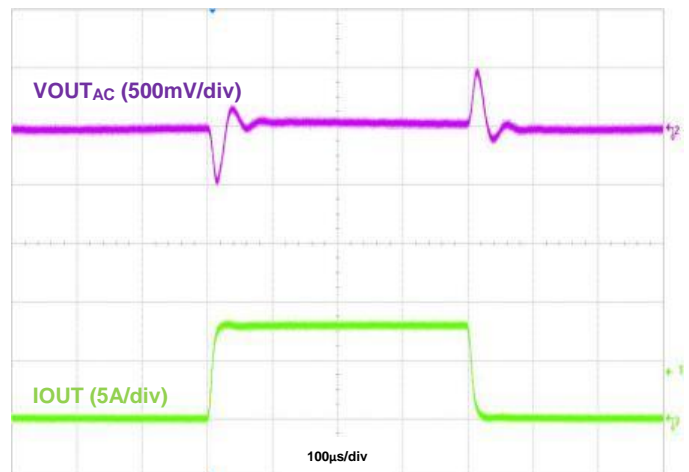


Figure 46. Load Transient,  $I_{OUT} = 50\text{mA}$  to  $8\text{A}$  to  $50\text{mA}$



## Application Information

### 1 Pulse Width Modulation (PWM) Operation

The AP62800 device is a 4.5V-to-17V input, 8A output, EMI friendly, fully integrated synchronous buck converter. Refer to the block diagram in Figure 4. The device employs constant on-time control to provide fast transient response and easy loop stabilization. At the beginning of each cycle, the one-shot pulse turns on the high-side power MOSFET, Q1, for a fixed on-time,  $t_{ON}$ . This one-shot on-pulse timing is calculated by the converter's input voltage and output voltage to maintain a pseudo-fixed frequency over the input voltage range. When Q1 is on, the inductor current rises linearly and the device charges the output capacitor. Q1 turns off after the fixed on-time expires, and the low-side power MOSFET, Q2, turns on. Once the output voltage drops below the output regulation, Q2 turns off. The one-shot timer is then reset and Q1 turns on again. The on-time is inversely proportional to the input voltage and directly proportional to the output voltage. It is calculated by the following equation:

$$t_{ON} = \frac{V_{OUT}}{V_{IN} \cdot f_{SW}} \quad \text{Eq. 1}$$

Where:

- $V_{IN}$  is the input voltage
- $V_{OUT}$  is the output voltage
- $f_{SW}$  is the switching frequency

The off-time duration is  $t_{OFF}$  and starts after the on-time expires. The off-time expires when the feedback voltage decreases below the reference voltage, which then triggers the on-time duration to start again. The minimum off-time is 255ns typical.

Connecting the MODE pin to VCC programs the device to operate in PWM Mode regardless of output load.

### 2 Pulse Frequency Modulation (PFM) and Ultrasonic Mode (USM) Operation

AP62800 enters PFM operation at light load conditions for high efficiency when the MODE pin is tied to GND. During light load conditions, the regulator automatically reduces the switching frequency. As the output current decreases, so too does the inductor current. The inductor current,  $I_L$ , eventually reaches 0A, marking the boundary between Continuous Conduction Mode (CCM) and Discontinuous Condition Mode (DCM). During this time, both Q1 and Q2 are off, and the load current is provided only by the output capacitor. When  $V_{FB}$  becomes lower than 0.6V, the next cycle begins, and Q1 turns on.

Likewise, as the output load increases from light load to heavy load, the switching frequency increases to maintain the regulation of the output voltage. The transition point between light and heavy load conditions can be calculated using the following equation:

$$I_{LOAD} = \left( \frac{V_{IN} - V_{OUT}}{2L} \right) \cdot t_{ON} \quad \text{Eq. 2}$$

Where:

- $L$  is the inductor value

AP62800 enters USM during light load conditions when the MODE pin is left floating. USM is similar to PFM Mode but with one key difference. Unlike in PFM Mode, operating in USM limits the switching frequency of the device from going below 22kHz. This prevents the device from switching in the audible frequency range. When the regulator detects that no switching has occurred within the last 35μs, it turns on Q2 for a fixed amount of time to force switching action on SW.

The quiescent current of AP62800 is 195μA typical under a no-load, non-switching condition.

## Application Information (continued)

### 3 Enable

When disabled, the device shutdown supply current is only 1μA. When applying a voltage greater than the EN logic high threshold (typical 1.2V, rising), the AP62800 enables all functions and the device initiates the soft-start phase. An internal 1.4μA pull-up current source connected from the internal LDO-regulated VCC to the EN pin guarantees that if EN is left floating, the device is still automatically enabled once the voltage reaches the EN logic high threshold. The AP62800 has a built-in 1ms soft-start time to prevent output voltage overshoot and inrush current. The soft-start time is also programmable by connecting an external capacitor from SS/TR to GND. See **Soft-start, Tracking, and Sequencing** section for more details. When the EN voltage falls below its logic low threshold (typical 1.12V, falling), the internal SS voltage discharges to ground and device operation is disabled.

The EN pin can also be used to program the undervoltage lockout thresholds. See **Adjusting Undervoltage Lockout (UVLO)** section for more details.

### 4 Soft-Start, Tracking, and Sequencing

When the SS/TR pin is left floating, the AP62800 uses its built-in soft-start time,  $t_{ss}$ , of 1ms. The soft-start time can be extended by connecting an external capacitor from SS/TR to GND. The capacitor, along with the internal  $I_{ss}$  of 5μA, determines the new soft-start time. The capacitance required for a given programmed soft-start time is calculated by:

$$C_{SS}[\text{nF}] = 8.33 \cdot t_{ss}[\text{ms}] \quad \text{Eq. 3}$$

Where:

- $C_{ss}$  is the soft-start capacitance in nF
- $t_{ss}$  is the soft-start time in ms

Two AP62800 devices, IC#1 and IC#2, can be used in a ratiometric tracking configuration. Each AP62800 device shares the same  $C_{ss}$  capacitance, which programs the same soft-start time for each device. See Figure 47 and Figure 48 for more details.

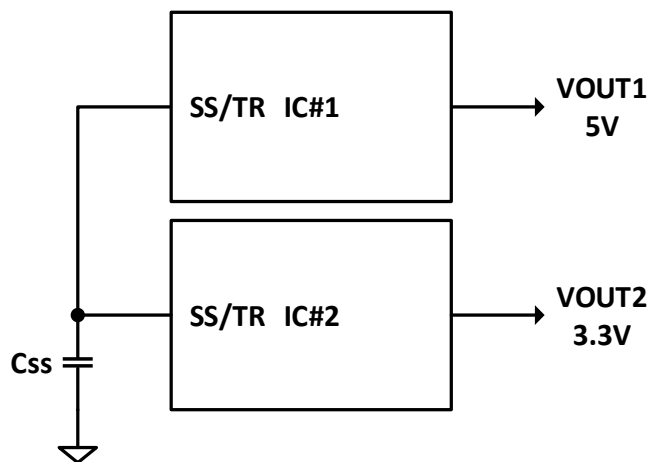


Figure 47. Ratiometric Tracking Configuration

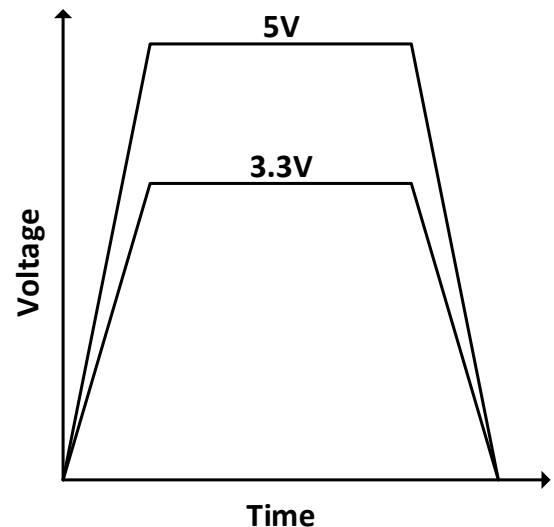


Figure 48. Ratiometric Tracking Function



## Application Information (continued)

### 4 Soft-Start, Tracking, and Sequencing (continued)

Two AP62800 devices can be used in a coincidental tracking configuration. The higher voltage output of IC#1 is divided down to connect to the input of IC#2's SS/TR pin, which overrides IC#2's internal 0.6V reference voltage during start-up. Each AP62800 device has the same output voltage rising and falling slew rates. The resistive divider (R5 and R6) should have a ratio that matches the ratio of the feedback resistive divider of IC#2. See Figure 49 and Figure 50 for more details.

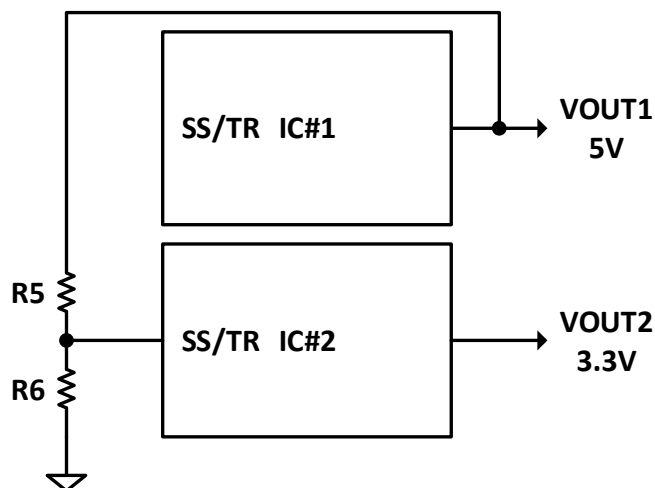


Figure 49. Coincidental Tracking Configuration

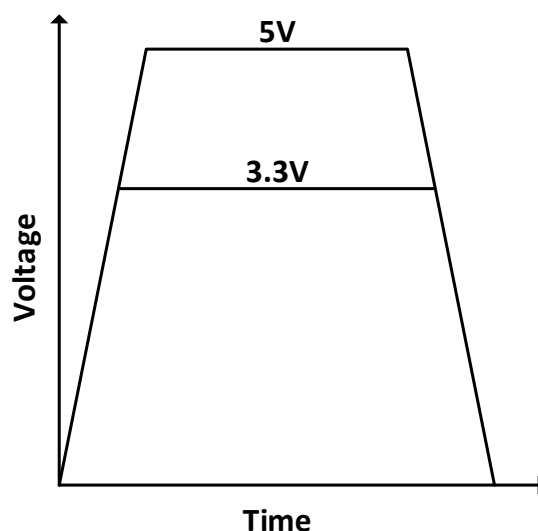


Figure 50. Coincidental Tracking Function

Two AP62800 devices can be used in an output sequencing configuration. Once the output voltage of IC#1 is within regulation, its PG signal goes from low to high and enables the start-up sequence of IC#2. See Figure 51 and Figure 52 for more details.

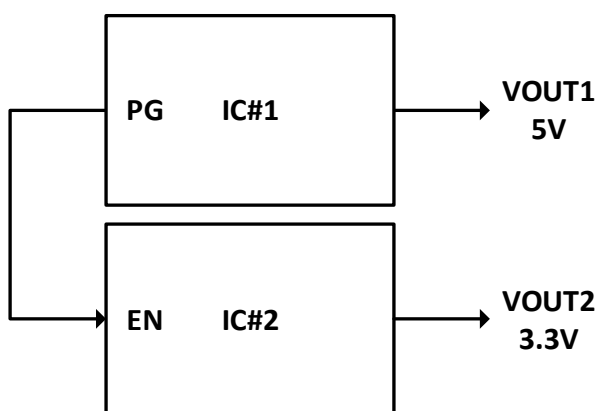


Figure 51. Output Sequencing Configuration

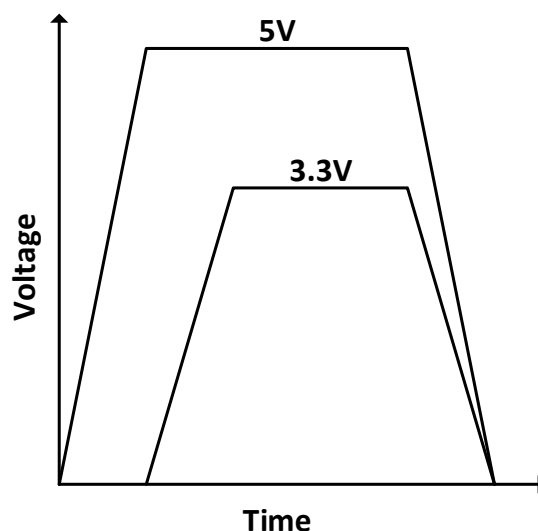


Figure 52. Output Sequencing Function

### 5 Electromagnetic Interference (EMI) Reduction with Ringing-Free Switching Node

In some applications, the system must meet EMI standards. In relation to high frequency radiation EMI noise, the switching node's (SW's) ringing amplitude is especially critical. To dampen high frequency radiated EMI noise, the AP62800 device implements a proprietary, multi-level gate driver scheme that achieves a ringing-free switching node without sacrificing the switching node's rise and fall slew rates as well as the converter's power efficiency.

## Application Information (continued)

### 6 Power-Good (PG) Indicator

The PG pin of AP62800 is an open-drain output that is actively held low during the soft-start period until the output voltage reaches 95% of its target value. When the output voltage is outside of its regulation by  $\pm 15\%$ , PG pulls low until the output returns within 5% of its set value. The PG rising edge transition is delayed by 0.5ms. An internal pull-up resistor of  $5M\Omega$  connects PG to VCC.

### 7 Adjusting Undervoltage Lockout (UVLO)

Undervoltage lockout is implemented to prevent the IC from insufficient input voltages. The AP62800 device has a UVLO comparator that monitors the input voltage and the internal bandgap reference. The AP62800 is disabled if the input voltage falls below 3.95V. In this UVLO event, both the high-side and low-side power MOSFETs turn off.

Some applications may desire higher VIN UVLO threshold voltages than is provided by the default setup. A  $3.7\mu A$  hysteresis pull-up current source on the EN pin along with an external resistive divider (R3 and R4) configures the VIN UVLO threshold voltages as shown in Figure 53.

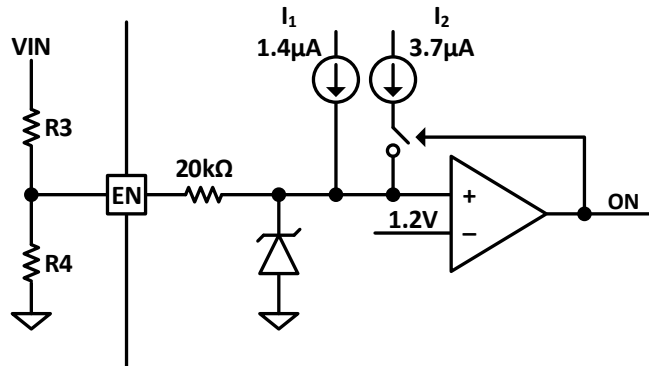


Figure 53. Adjusting UVLO

The resistive divider resistor values are calculated by:

$$R3 = \frac{0.933 \cdot V_{ON} - V_{OFF}}{3.793\mu A} \quad \text{Eq. 4}$$

$$R4 = \frac{1.12 \cdot R3}{V_{OFF} - 1.12V + 5.1\mu A \cdot R3} \quad \text{Eq. 5}$$

Where:

- $V_{ON}$  is the rising edge VIN voltage to enable the regulator and is greater than 4.45V
- $V_{OFF}$  is the falling edge VIN voltage to disable the regulator and is greater than 4.15V

### 8 Overcurrent Protection (OCP)

The AP62800 has cycle-by-cycle valley current limit protection by sensing the current through the internal low-side power MOSFET, Q2. While Q2 is on, the internal sensing circuitry monitors its conduction current. The overcurrent limit has a corresponding voltage limit,  $V_{LIMIT}$ . When the voltage between GND and SW is lower than  $V_{LIMIT}$  due to excessive current through Q2, the OCP is triggered, and the controller turns off Q2. During this time, both Q1 and Q2 remain off. A new switching cycle begins only when the voltage between GND and SW rises above  $V_{LIMIT}$ . If Q2 consistently hits the valley current limit for 1- $t_{SS}$ , the buck converter enters hiccup mode and shuts down. After 7- $t_{SS}$  of down time, the buck converter restarts powering up. Hiccup mode reduces the power dissipation in the overcurrent condition.

Because the  $R_{DS(ON)}$  values of the power MOSFETs increase with temperature,  $V_{LIMIT}$  has a temperature coefficient of  $0.4\%/^{\circ}C$  to compensate for the temperature dependency of  $R_{DS(ON)}$ .

## Application Information (continued)

### 9 Thermal Shutdown (TSD)

If the junction temperature of the device reaches the thermal shutdown limit of +160°C, the AP62800 shuts down both its high-side and low-side power MOSFETs. When the junction temperature reduces to the required level (+130°C typical), the device initiates a normal power-up cycle with soft-start.

### 10 Power Derating Characteristics

To prevent the regulator from exceeding the maximum recommended operating junction temperature, some thermal analysis is required. The regulator's temperature rise is given by:

$$T_{\text{RISE}} = PD \cdot (\theta_{JA}) \quad \text{Eq. 6}$$

Where:

- PD is the power dissipated by the regulator
- $\theta_{JA}$  is the thermal resistance from the junction of the die to the ambient temperature

The junction temperature,  $T_J$ , is given by:

$$T_J = T_A + T_{\text{RISE}} \quad \text{Eq. 7}$$

Where:

- $T_A$  is the ambient temperature of the environment

For the V-QFN2030-12 (Type A) package, the  $\theta_{JA}$  is 40°C/W. The actual junction temperature should not exceed the maximum recommended operating junction temperature of +125°C when considering the thermal design. Figure 54 shows a typical derating curve versus ambient temperature.

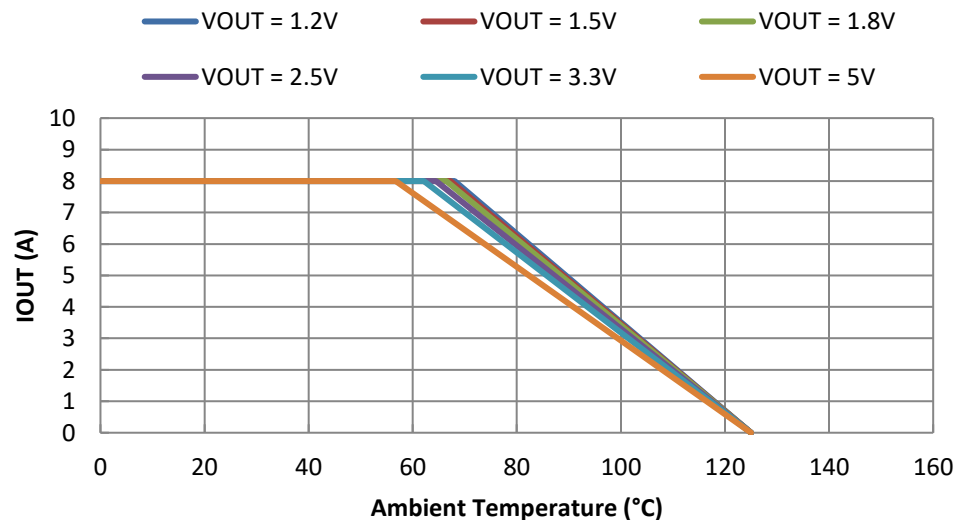


Figure 54. Output Current Derating Curve vs. Ambient Temperature, VIN = 12V, fsw = 800kHz

## Application Information (continued)

### 11 Setting the Output Voltage

The AP62800 has an adjustable output voltage, starting from 0.6V, using an external resistive divider. The resistor values of the feedback network are selected based on a design trade-off between efficiency and output voltage accuracy. There is less current consumption in the feedback network for high resistor values, which improves efficiency at light loads. However, values too high cause the device to be more susceptible to noise affecting its output voltage accuracy. R1 can be determined by the following equation:

$$R1 = R2 \cdot \left( \frac{V_{OUT}}{0.6V} - 1 \right) \quad \text{Eq. 8}$$

Table 1 shows a list of recommended component selections for common AP62800 output voltages referencing Figure 1. The AP62800 is capable of delivering output voltages greater than the listed maximum recommended output voltage of 7.0V by modifying the typical application circuit with additional external components. Consult Diodes Incorporated for more information if such output voltages are required.

**Table 1. Recommended Component Selections**

AP62800							
Output Voltage (V)	Frequency (kHz)	R1 (kΩ)	R2 (kΩ)	L (μH)	C1 (μF)	C2 (μF)	C3 (nF)
1.2	400	30.1	30.1	1.00	22	4 x 22	100
	800			0.47			
	1200			0.33			
1.5	400	45.3	30.1	1.10	22	4 x 22	100
	800			0.56			
	1200			0.39			
1.8	400	60.4	30.1	1.30	22	4 x 22	100
	800			0.68			
	1200			0.43			
2.5	400	95.3	30.1	1.60	22	4 x 22	100
	800			0.82			
	1200			0.56			
3.3	400	137.0	30.1	2.00	22	4 x 22	100
	800			1.00			
	1200			0.68			
5.0	400	221.0	30.1	2.40	22	4 x 22	100
	800			1.20			
	1200			0.95			

## Application Information (continued)

### 12 Inductor

Calculating the inductor value is a critical factor in designing a buck converter. For most designs, the following equation can be used to calculate the inductor value:

$$L = \frac{V_{OUT} \cdot (V_{IN} - V_{OUT})}{V_{IN} \cdot \Delta I_L \cdot f_{sw}} \quad \text{Eq. 9}$$

Where:

- $\Delta I_L$  is the inductor current ripple
- $f_{sw}$  is the buck converter switching frequency

For AP62800, choose  $\Delta I_L$  to be 30% to 50% of the maximum load current of 8A.

The inductor peak current is calculated by:

$$I_{LPEAK} = I_{LOAD} + \frac{\Delta I_L}{2} \quad \text{Eq. 10}$$

Peak current determines the required saturation current rating, which influences the size of the inductor. Saturating the inductor decreases the converter efficiency while increasing the temperatures of the inductor and the internal power MOSFETs. Therefore, choosing an inductor with the appropriate saturation current rating is important. For most applications, it is recommended to select an inductor of approximately 0.33 $\mu$ H to 3.3 $\mu$ H with a DC current rating of at least 35% higher than the maximum load current. For highest efficiency, the inductor's DC resistance should be less than 5m $\Omega$ . Use a larger inductance for improved efficiency under light load conditions.

### 13 Input Capacitor

The input capacitor reduces both the surge current drawn from the input supply as well as the switching noise from the device. The input capacitor must sustain the ripple current produced during the on-time of Q1. It must have a low ESR to minimize power dissipation due to the RMS input current.

The RMS current rating of the input capacitor is a critical parameter and must be higher than the RMS input current. As a rule of thumb, select an input capacitor with an RMS current rating greater than half of the maximum load current.

Due to large  $di/dt$  through the input capacitor, electrolytic or ceramic capacitors with low ESR should be used. If using a tantalum capacitor, it must be surge protected or else capacitor failure could occur. Using a ceramic capacitor of 22 $\mu$ F or greater is sufficient for most applications.

### 14 Output Capacitor

The output capacitor keeps the output voltage ripple small, ensures feedback loop stability, and reduces both the overshoots and undershoots of the output voltage during load transients. During the first few microseconds of an increasing load transient, the converter recognizes the change from steady-state and sets the off-time to minimum to supply more current to the load. However, the inductor limits the change to increasing current depending on its inductance. Therefore, the output capacitor supplies the difference in current to the load during this time. Likewise, during the first few microseconds of a decreasing load transient, the converter recognizes the change from steady-state and increases the off-time to reduce the current supplied to the load. However, the inductor limits the change in decreasing current as well. Therefore, the output capacitor absorbs the excess current from the inductor during this time.

## Application Information (continued)

### 14 Output Capacitor (continued)

The effective output capacitance, COUT, requirements can be calculated from the equations below.

The ESR of the output capacitor dominates the output voltage ripple. The amount of ripple can be calculated by:

$$V_{OUT\_Ripple} = \Delta I_L \cdot \left( ESR + \frac{1}{8 \cdot f_{SW} \cdot C_{OUT}} \right) \quad \text{Eq. 11}$$

An output capacitor with large capacitance and low ESR is the best option. For most applications, a total capacitance of 4 x 22μF using ceramic capacitors is sufficient. To meet the load transient requirements, the calculated COUT should satisfy the following inequality:

$$C_{OUT} > \max \left( \frac{L \cdot I_{Trans}^2}{\Delta V_{Overshoot} \cdot V_{OUT}}, \frac{L \cdot I_{Trans}^2}{\Delta V_{Undershoot} \cdot (V_{IN} - V_{OUT})} \right) \quad \text{Eq. 12}$$

Where:

- $I_{Trans}$  is the load transient
- $\Delta V_{Overshoot}$  is the maximum output overshoot voltage
- $\Delta V_{Undershoot}$  is the maximum output undershoot voltage

### 15 Bootstrap Capacitor

To ensure proper operation, a ceramic capacitor must be connected between the BST and SW pins to supply the drive voltage for the high-side power MOSFET. A 100nF ceramic capacitor is sufficient.

## Layout

### PCB Layout

1. The AP62800 works at 8A load current so heat dissipation is a major concern in the layout of the PCB. 2oz copper for both the top and bottom layers is recommended.
2. Place the input capacitors as closely across VIN and PGND as possible.
3. Place the inductor as close to SW as possible.
4. Place the output capacitors as close to PGND as possible.
5. Place the feedback components as close to FB as possible.
6. If using four or more layers, use at least the 2<sup>nd</sup> and 3<sup>rd</sup> layers as PGND to maximize thermal performance.
7. Add as many vias as possible around both the PGND pin and under the PGND plane for heat dissipation to all the PGND layers.
8. Add as many vias as possible around both the VIN pin and under the VIN plane for heat dissipation to all the VIN layers.
9. See Figure 55 for more details.

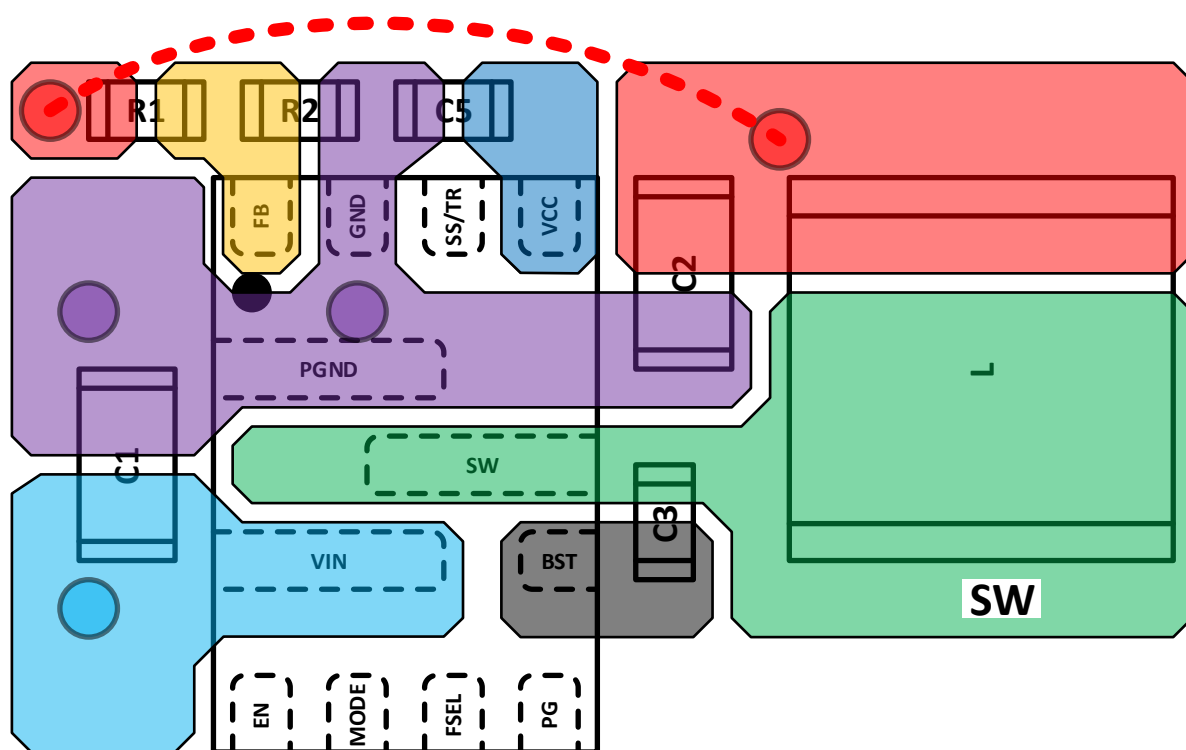
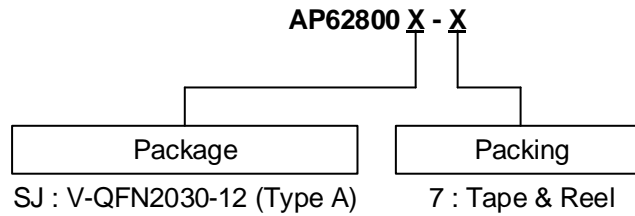


Figure 55. Recommended PCB Layout

## Ordering Information

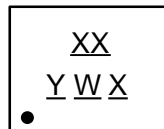


Part Number	Part Number Suffix	Package	Package Code	Packing	
				Qty.	Carrier
AP62800SJ-7	-7	V-QFN2030-12 (Type A)	SJ	3,000	Tape and Reel

## Marking Information

V-QFN2030-12 (Type A)

( Top View )



XX : Identification Code  
Y : Year : 0 to 9 (ex: 2 = 2022)  
W : Week : A to Z : week 1 to 26;  
a to z : week 27 to 52; z represents  
week 52 and 53  
X : Internal Code

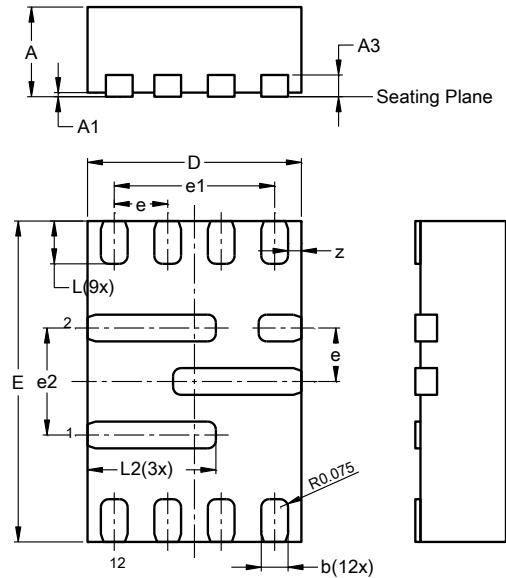
Part Number	Package	Identification Code
AP62800SJ-7	V-QFN2030-12 (Type A)	KD



## Package Outline Dimensions

Please see <http://www.diodes.com/package-outlines.html> for the latest version.

V-QFN2030-12 (Type A)

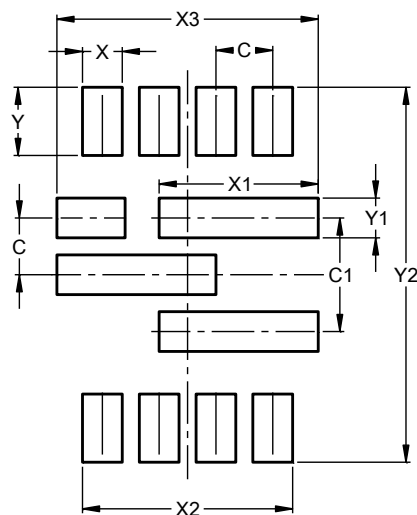


V-QFN2030-12 (Type A)			
Dim	Min	Max	Typ
A	0.75	0.85	0.80
A1	0.00	0.05	0.02
A3	—	—	0.203
b	0.20	0.30	0.25
D	1.95	2.05	2.00
E	2.95	3.05	3.00
e	0.50 BSC		
e1	1.50 BSC		
e2	1.00 BSC		
L	0.35	0.45	0.40
L2	1.15	1.25	1.20
z	—	—	0.125
All Dimensions in mm			

## Suggested Pad Layout

Please see <http://www.diodes.com/package-outlines.html> for the latest version.

V-QFN2030-12 (Type A)



Dimensions	Value (in mm)
C	0.500
C1	1.000
X	0.350
X1	1.400
X2	1.850
X3	2.300
Y	0.600
Y1	0.350
Y2	3.300

## Mechanical Data

- Moisture Sensitivity: Level 1 per J-STD-020
- Terminals: Finish – SnAgCu Plated, Solderable per MIL-STD-202, Method 208 ①
- Weight: 0.0114 grams (Approximate)

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